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Microwave Journal

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Military and Government Electronics

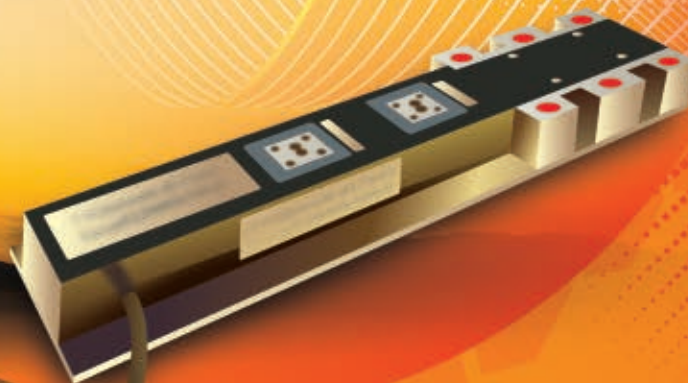
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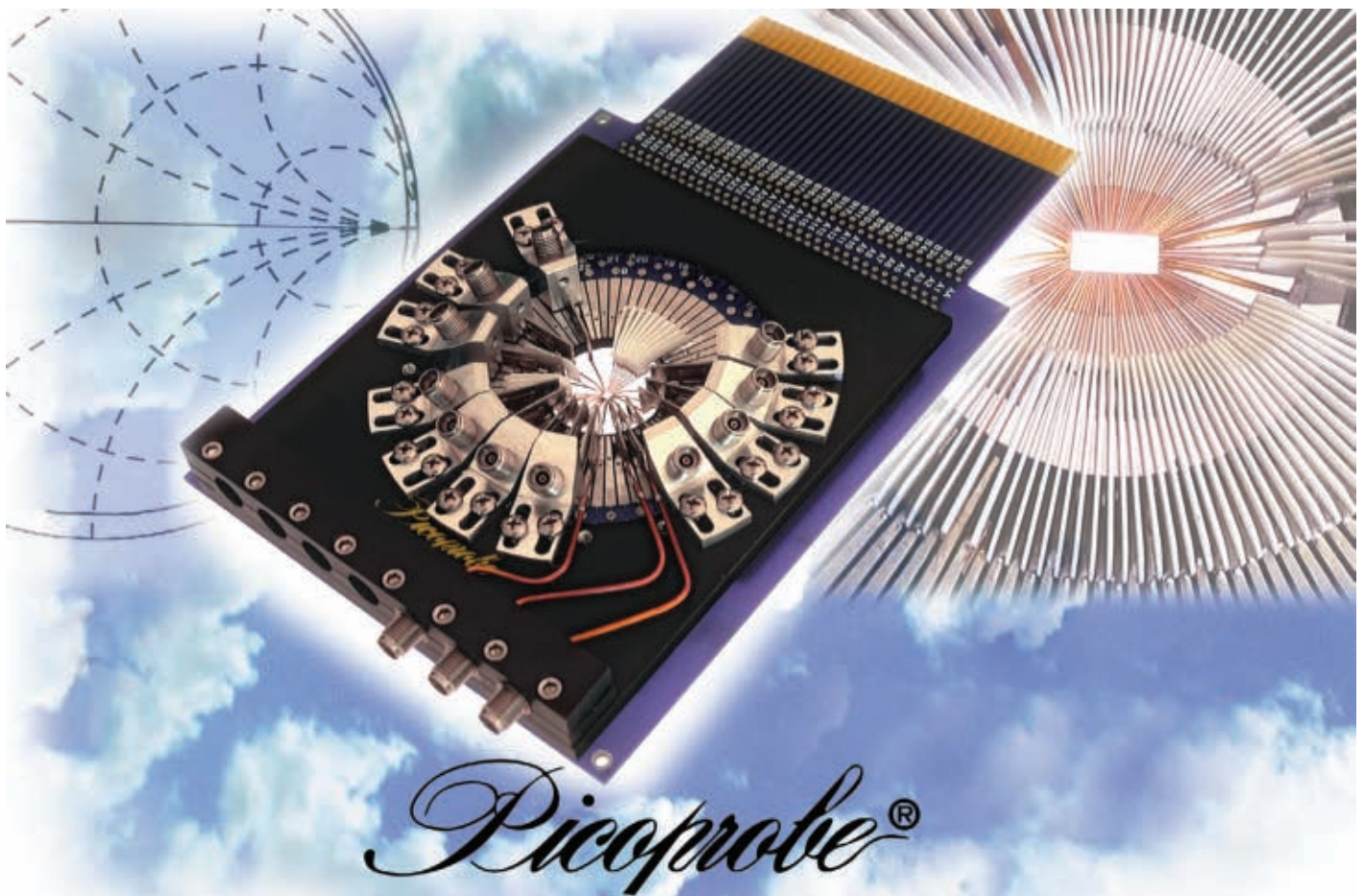
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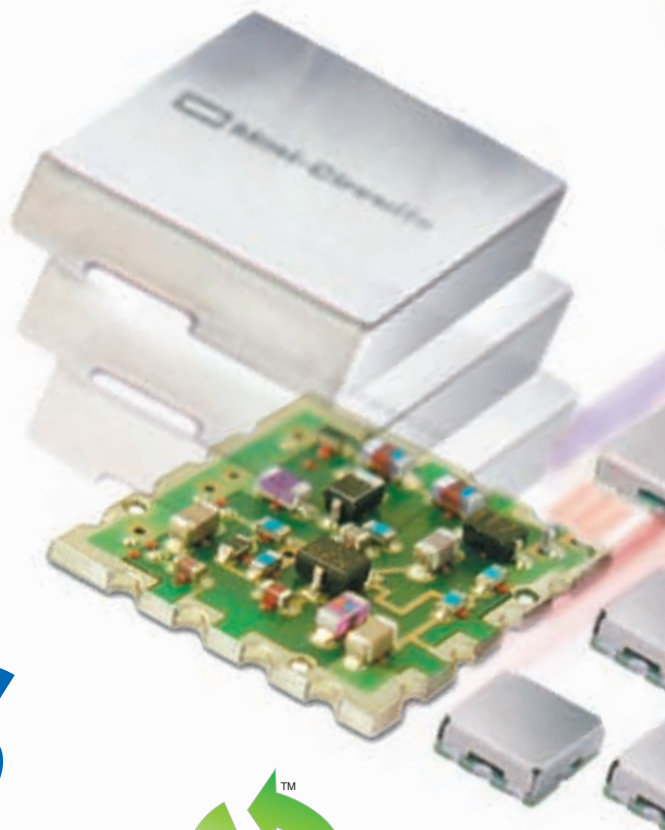
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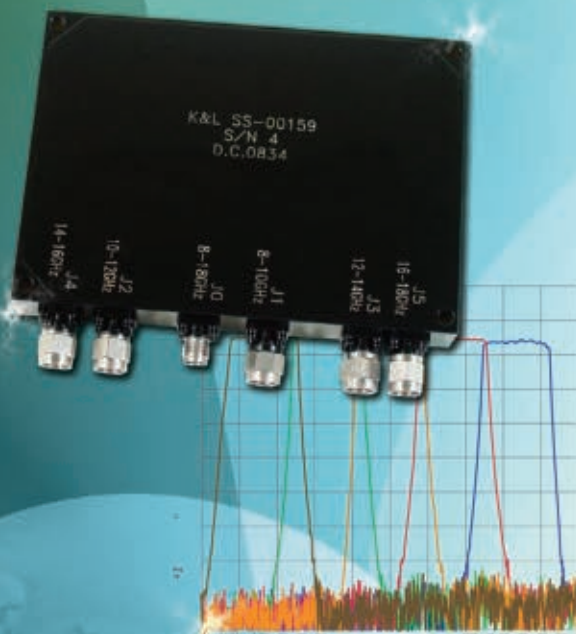
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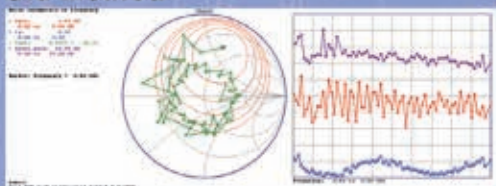
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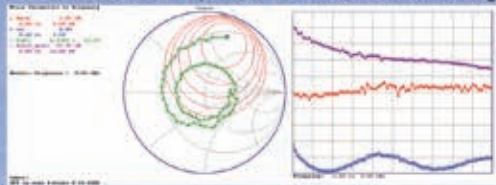
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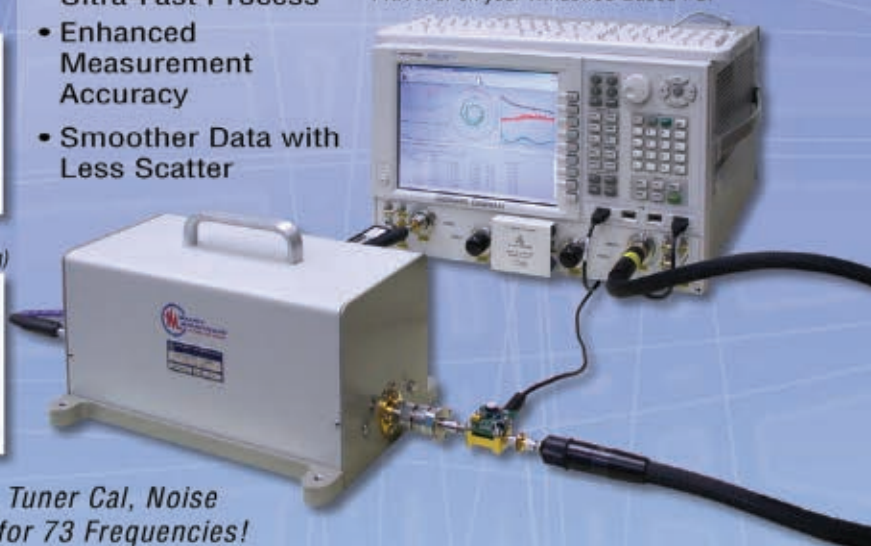
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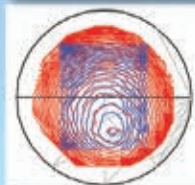
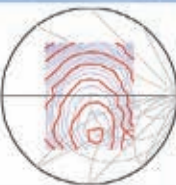
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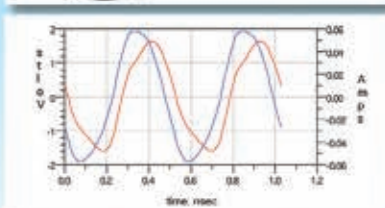


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COVER FEATURE: THEN AND NOW

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Ervin J. Nalos, General Electric Co.

This article, first published in December of 1959, emphasized the interaction of linear beam circuits with periodically loaded waveguides

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Brian Coaker and Tony Challis, e2v

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Richard Mumford, Microwave Journal International Editor

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104 A Microwave Journey, Part IV: The 1980s

David Vye, Editor, Microwave Journal

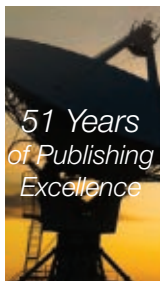
Fourth in a multi-part series dedicated to a decade-by-decade breakdown of the history of *Microwave Journal*

TECHNICAL FEATURES

116 An Approach for Determining MOSFET Small-signal Circuit Model Parameters

Qian Wang, Cheng Yuan and Yasen Huang, Southeast University; Jianjun Gao, East China Normal University

Proposed method to extract the small-signal model parameters of a metal-oxide semiconductor field effect transistor



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M.J. Poulton, K. Krishnamurthy, J. Martin, B. Landberg, R. Vetury and D. Aichele, RF Micro Devices

Demonstration of a 400 W power amplifier operating at 65 V with better than 48.4 percent drain efficiency over a 600 MHz bandwidth from 2.9 to 3.5 GHz

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Mark Winebrand and John Aubin, ORBIT/FR Inc.

Implementation of a full 3-D simulation technique for anechoic chambers at low frequencies using a commercial transient solver package

150 A Compact CPW-fed Rectangle-trapezoid-rectangle Shaped Monopole Antenna for Ultra-wideband Systems

Wen-Shan Chen and Kai-Cheng Yang, Southern Taiwan University

Presentation of a coplanar waveguide-fed rectangle-trapezoid-rectangle shape monopole antenna designed to reduce size, improve impedance bandwidth and smooth gain

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Design of highly integrated chipsets for the frequency range between 5 to 16 GHz

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Rohde & Schwarz

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CST of America

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HUBER+SUHNER AG

Introduction to a microwave cable assembly family designed for the test and measurement, defense, instrumentation and space markets

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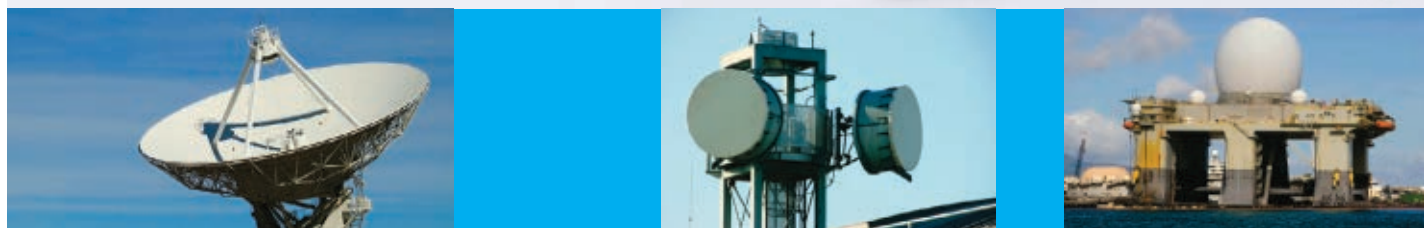
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Executive Interview

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Retrospectives: An excerpt from the new book by Norman H. Pond, *The Tube Guys*. Pond was a tube guy for 30 years - with Hughes Aircraft, Sylvania, Microwave Electronics and eventually as president of Varian. The author of several articles on this topic for MWJ, Pond has now authored a truly fascinating history on this technology's evolution.

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Online Technical Papers

Novel Compact Monopole Antenna with a Parasitic Plate for WLAN Applications

Wen-Shan Chen and Ho-Yu Lin, Southern Taiwan University of Technology

Application Note: Designing GaAs Power Amplifiers for Femtocells

Joe Cozzarelli, Anadigics

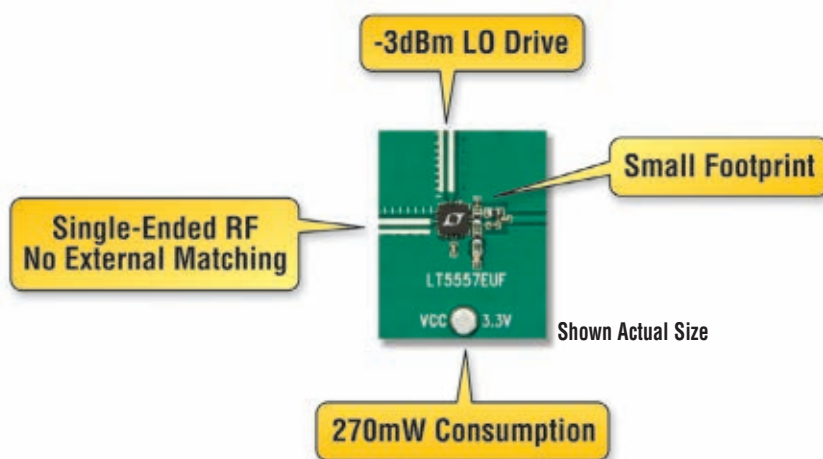
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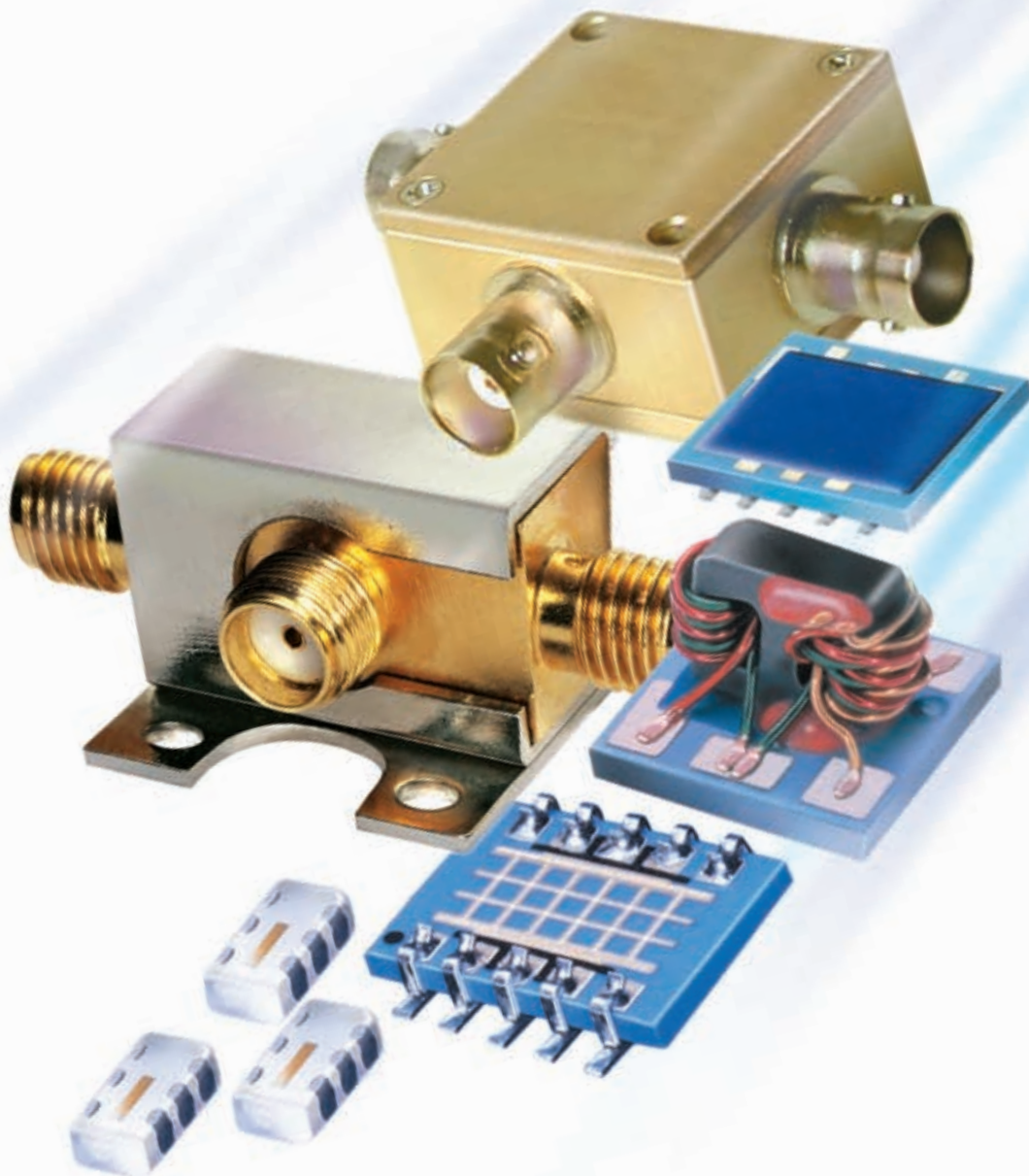


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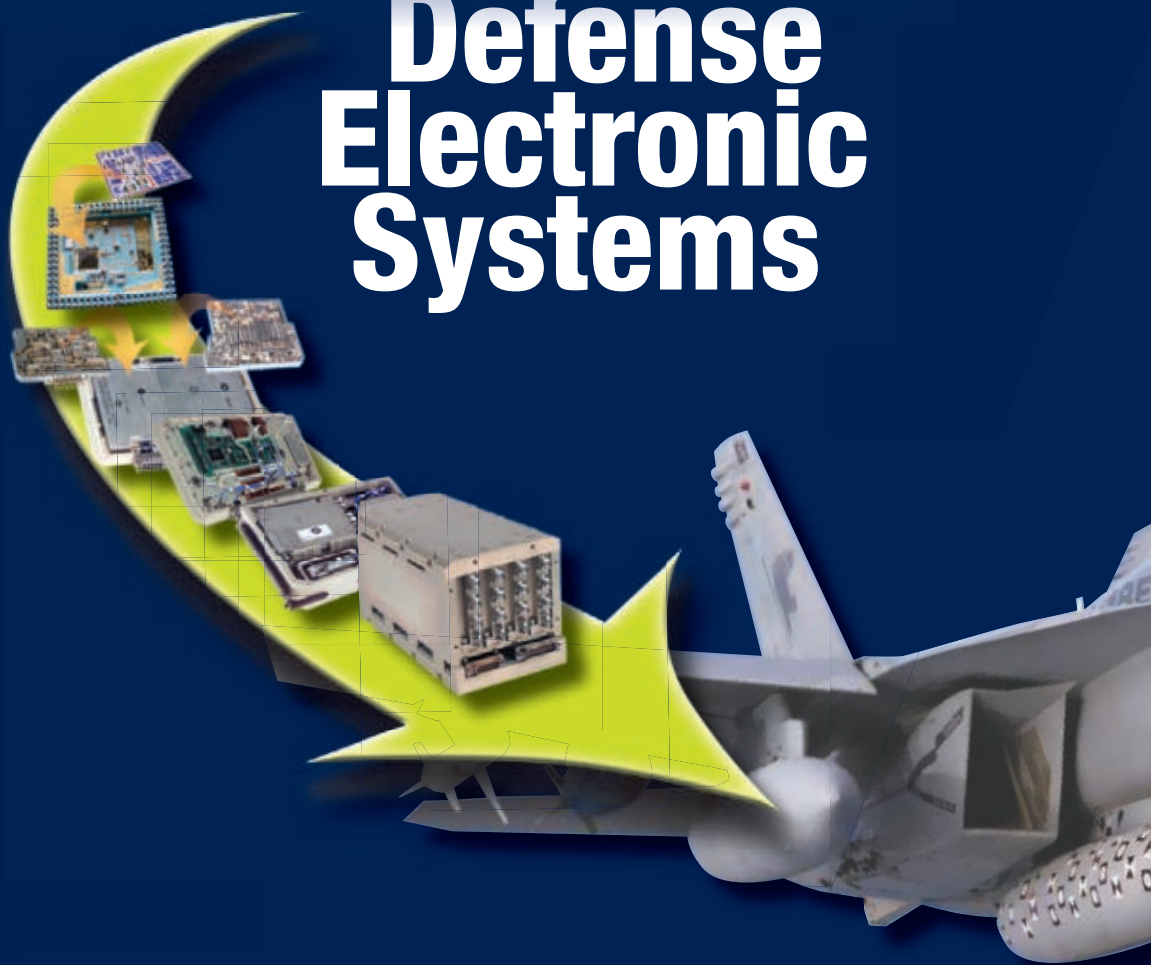
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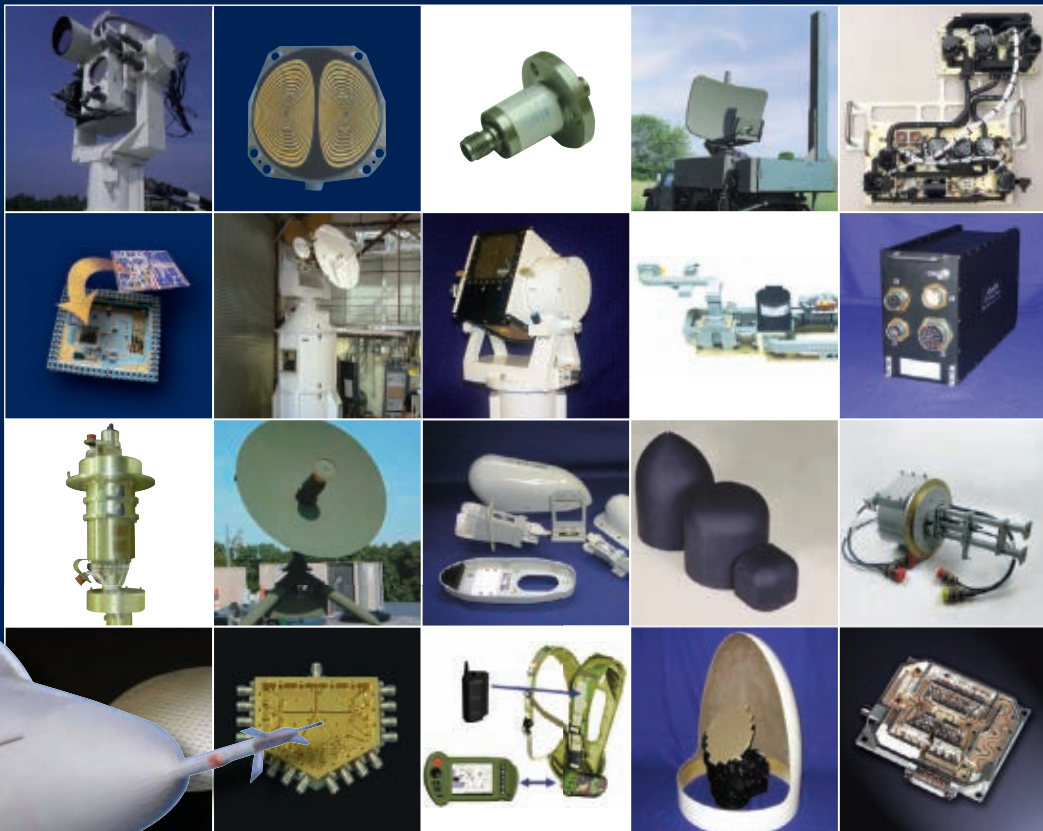


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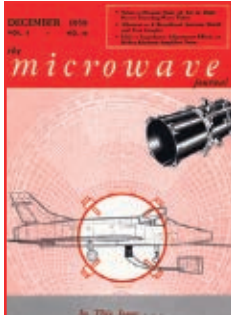
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PRESENT STATE OF ART IN HIGH POWER TRAVELING-WAVE TUBES

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General Electric Co.
Microwave Laboratory
Palo Alto, California

ABSTRACT

The object of this paper is to outline the present state of art in the high power microwave field with special emphasis on linear beam circuits interacting with periodically loaded waveguides.

A number of interaction circuits are discussed, both for "O" and "M" type tubes and areas of advances and future trends are indicated.

I. INTRODUCTION

A. Historical Background

The present effort in the area of high power traveling-wave tubes finds its common root in both klystron development and the original low power helix TWT development. This is in a sense natural, since the achievement of megawatt-type microwave devices was first demonstrated in a klystron¹ whereas broadband amplification was first demonstrated in the low power helix TW tube.² Both types of devices use the velocity modulation principle, one in the form of standing waves, the other in the form of traveling-waves. In addition, many similarities in the design of both devices, such as beam formation, extraction of electromagnetic energy, and beam collection, serve to provide a common background of development. The discussion in this paper will deal primarily with linear beam devices with some reference to cross-field devices in order to give a fairly comprehensive picture of the state of art in high power microwave tubes.

The first effort designed to produce megawatts of pulsed
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microwave power was conducted on the high power pulsed klystron³ at Stanford. This work conclusively demonstrated that large oxide-coated cathodes could be operated reliably at voltages of several hundred kilovolts, and provided the necessary impetus for further high power research directed toward the achievement of broader bandwidth at high power levels. Although prior to this work, a number of interaction circuits have been suggested by Pierce,⁴ Field,⁵ and others, their electrical characteristics were considered inferior to the simple helix at all but the highest voltages, where the helix becomes unsuitable. This is primarily due to its good radiating properties when stretched out to be in synchronism with a high velocity beam. With the demonstrated success of the high power pulsed klystron, a much greater interest developed in the utilization of traveling-wave devices in conjunction with high voltage electron beams. Unfortunately, in order to slow the electromagnetic wave down to synchronism with an electron beam, smooth transmission lines such as waveguides cannot be used directly; instead, some form of loading must be used. The periodically loaded waveguide provides a means of doing this.

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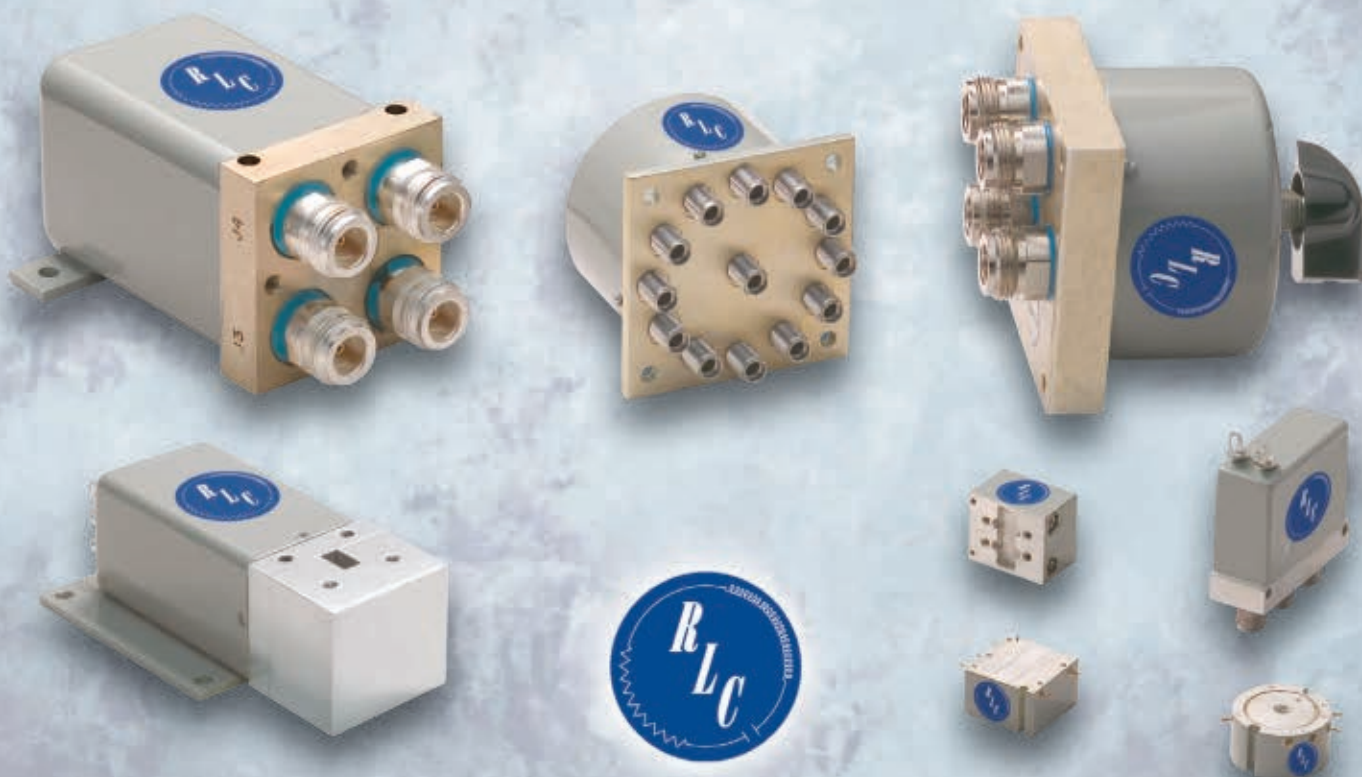
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B. General Discussions of High Power Microwave Tubes

Before proceeding with a detailed analysis of the periodically loaded waveguide, which has proved to be so important in the high power TW tube field, it is appropriate to discuss briefly the present state of art in all types of high power microwave tubes. This is outlined in Table I. Klystrons with their inherently high gain, low power TW tubes with their large bandwidth, and magnetron-like devices with their high efficiency, have all invaded the high power field. It is clear that keen competition between these devices will continue and that no single approach will satisfy all the foreseen needs. As indicated in Table I, hybrid devices exploiting the advantages of two or more different types of interaction may well provide a solution to some of the problems encountered to date.

	KLYSTRON			MAGNETRON		TW TUBE		
A. General Performance	Gain, db	Power, Watt	Efficiency, %	Frequency, Mc	Power, Watt	Gain, db	Power, Watt	Efficiency, %
Gain	40-60		80-90	10-100	10-100	10-100	10-100	10-100
Power	10-100	10-100	10-100	10-100	10-100	10-100	10-100	10-100
Efficiency	10-100	10-100	10-100	10-100	10-100	10-100	10-100	10-100
Frequency	10-100	10-100	10-100	10-100	10-100	10-100	10-100	10-100
Bandwidth	10-100	10-100	10-100	10-100	10-100	10-100	10-100	10-100
Stability	10-100	10-100	10-100	10-100	10-100	10-100	10-100	10-100
Range, Power	10-100	10-100	10-100	10-100	10-100	10-100	10-100	10-100
B. Special Features								
1. Beam-Current	Constant Beam, Low Beam Current			Variable Beam, High Beam Current		Variable Beam, High Beam Current		
2. Beam-Current	Constant Beam, Low Beam Current			Variable Beam, High Beam Current		Variable Beam, High Beam Current		
3. Beam-Current	Constant Beam, Low Beam Current			Variable Beam, High Beam Current		Variable Beam, High Beam Current		
4. Beam-Current	Constant Beam, Low Beam Current			Variable Beam, High Beam Current		Variable Beam, High Beam Current		

Table 1—High Power microwave tubes (S-Band).

The present effort to extend the state of art in these three fields has proceeded as follows:

1. The simple synchronously tuned multi-cavity klystron, capable of stable gains in excess of 60 db, has been adapted to provide means of detuning the intermediate cavities to give an increased bandwidth at some sacrifice in gain. Gains of 30-40 db have been obtained over a 3-5 per cent bandwidth at megawatt levels by staggering the initial cavities and broadbanding the output system by loading or the use of multiply-tuned cavities. Efficiencies of about 30 per cent are achievable in these types of tubes.

2. The crossed-field amplifier, with its inherently high efficiency (typically 40-50%) has given megawatts of peak power at the lower microwave frequencies, with CW capabilities in the range of hundreds of watts. Considerable effort is continuing to obtain better understanding of the complex interaction of the magnetron type with traveling-wave fields. A number of new slow-wave circuits for crossed-field devices are also being considered. There are no basic differences in the types of slow-wave circuits designed for linear-beam or crossed-field interaction except for the difference in synchronous voltage for a given power level. Perhaps the most distinguishing features of the crossed-field amplifier to date is its predominant op-

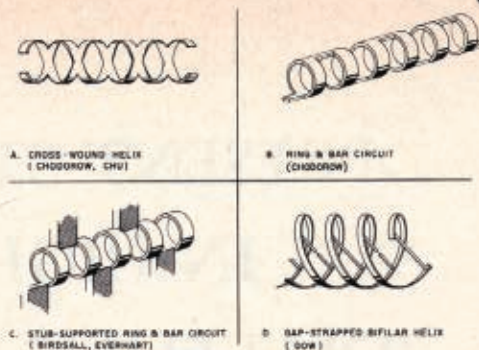


Figure 1—Some helix modifications for high power applications.

eration on a backward-wave, whereas all broadband "O" type traveling-wave amplifiers interact with a forward-wave.

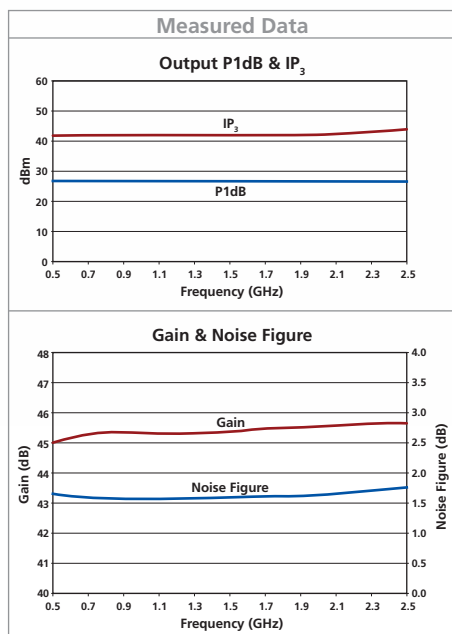
From the point of view of available current in the crossed field device, amplification can be achieved by either the use of an injected beam from outside of the r-f circuit, or by the use of a continuously emitting surface. The beam can be collected, or made re-entrant. It is not clear to date which of these two methods of current generation offer greater promise for higher power applications. Both types of injection have achieved stable gains in the 10-15 db region but the mechanism which limits the gain is not yet clearly understood.

3. The simple helix is still the most frequently employed slow-wave circuit in TW tubes. It has been used in low noise applications, in medium power amplifiers (with a CW capability as high as 10 watts at X-band), and in pulsed applications (as high as several kilowatts at S-band). In addition, it has found application in electronically tunable oscillators and amplifiers. Considerable work has been expended to modify the simple helix into circuits suitable for higher voltage interaction and higher average power capability. Some of these are shown in Figure 1. For example, a four helix circuit developed by Putz⁵ has made it possible to develop 100 watts of CW power at X-band over an almost 2:1 frequency range (see Figure 2).

The evolution of the contrawound helix² (Figure 1A) and its close relative, the "ring and bar" circuit^{6,7,8} (Figure 1B) have extended the useful range of operating voltages to the 20-70 kv range as well as allowing the use of larger transverse dimensions at a given frequency. Tens of kilowatts of peak power have been achieved with these circuits. The stub-supported helix (Figure 1C) appears capable of extending the average power range although at some sacrifice in bandwidth. Modified multifilar helices have also been suggested for high power TWT applications.⁹ One such modification, thought promising for large bandwidth at high peak powers is the gap-strapped bifilar helix shown in Figure 1D. These devices are illustrative of the advances in the field of helix-derived circuits. It appears, however, that in the 10-30 per cent

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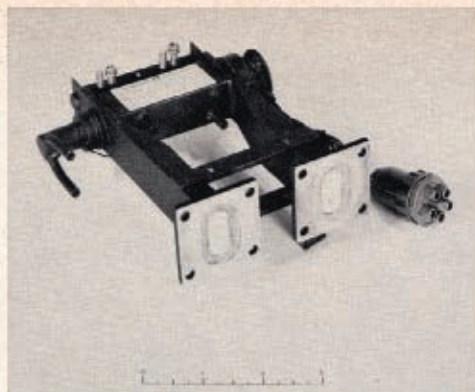


Figure 2—Z-5161 100 watt X-Band 4-Helix traveling-wave tube.

bandwidth region, the periodically loaded waveguide offers the greatest promise in achieving both high peak and average power simultaneously. The main emphasis of this paper lies in this area.

II. PERIODICALLY LOADED WAVEGUIDE CIRCUITS

A. General Considerations

The simple waveguide is basically a high pass filter, propagating energy with a phase velocity greater than light velocity at all frequencies. Any periodic loading of the circuit will result in cumulative reflections from the loading obstacles, which at some ranges of frequencies will cause total reflections, i.e., a stopband. The high pass filter thus becomes a bandpass filter, whose properties depend on the nature of the periodic loading. If the loading obstacles are small, little change from the waveguide characteristic will occur except near the regions of total reflections, curve 2, Figure 3. The new branches of the so-called "Brillouin" diagram (ω - β diagram) are required to fulfill the boundary conditions inside the composite circuit and are referred to as the spatial harmonics. They are mirror images of the fundamental passband and their amplitudes are determined by the detailed nature of the loading obstacles. If the loading is heavy, the waveguide passband is so greatly perturbed that it bears little relation to its original form. In many instances, it is convenient to visualize the slow-wave circuit as a set of resonant cavities coupled together by means of electric or magnetic fields. In the limit of zero coupling (no slots between cavities, or a resonant slot), the passband shrinks to zero, curve 4, Figure 3. With predominantly electric coupling (capacitive) the phase and group velocity in the first quadrant are of equal sign; giving curves 2 and 3, Figure 3; this is referred to as fundamental forward-wave interaction. With predominantly magnetic

coupling (positive inductive coupling), the group velocity in the first quadrant is of the opposite sign to the phase velocity (curve 5, Figure 3), and a fundamental backward-wave results. In the last case, for the next quadrant, ($\pi-2\pi$ phase shift), the group and phase velocities are of the same sign again, giving the so called spatial harmonic forward-wave interaction. The slope of the intersecting dotted line gives the V_p , while the slope of the ω - β curve itself at the operating point gives the V_g . In the forward wave, these are of the same sign. In the backward wave they are of opposite signs. For broadband operation, it is desirable to have the phase velocity nearly constant with frequency, i.e., low dispersion. It is seen in Figure 3, that in general, the fundamental forward-wave circuit is more dispersive than the spatial harmonic circuit, but the impedance is usually higher in the first quadrant since one is interacting with the main component of the r-f field.

A number of slow-wave circuits have evolved around the periodically loaded waveguide, both of the spatial harmonic type and of the fundamental forward-wave type. The first device of this type which employed interaction of a beam with a traveling-wave was the linear accelerator¹⁰ developed by Hansen at Stanford. This circuit is composed of a cylindrical pipe, periodically loaded by capacitive discs, whose phase velocity has been slowed down to the velocity of light (at midband) for purposes of accelerating an electron beam, rather than extracting energy from it, i.e., converting microwave energy into pulsed high voltage d.c. energy. The circuit has the properties of a passband filter whose bandwidth depends on the size of the coupling aperture. For the linear accelerator application, this is made very narrow; to obtain broadband characteristics the detailed nature of the coupling between the periodic obstacles must be examined. As contrasted with the simple helix, the periodically loaded waveguide offers some attractive features: it is rugged physically, and for a given frequency it is larger in size. Both these features tend to enhance its ultimate average power capabilities. On the other hand, due to the dispersive nature of the slow-wave circuit, the bandwidth tends to be limited. Although considerable attention has been given to various filter type circuits by Pierce,³ they were never seriously

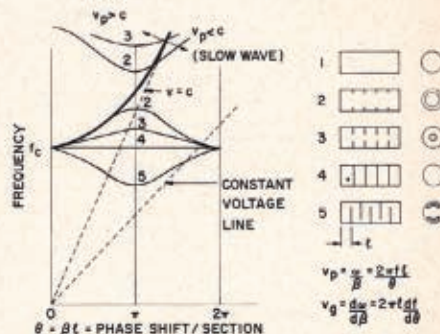
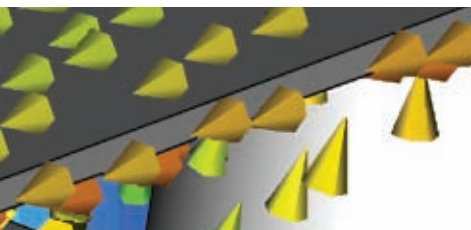


Figure 3—Brillouin Diagram (ω - β Diagram) for periodically loaded circuits.



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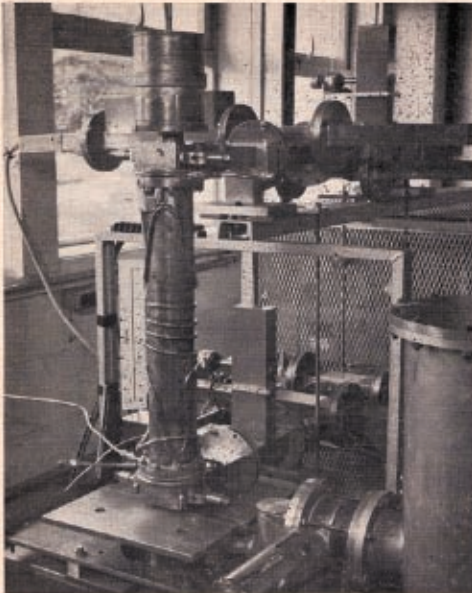


Figure 4—First S-Band Megawatt-type disc loaded TW tube (Stanford).

considered for TW amplification until interest arose in higher peak and average powers than could be achieved with helix-type circuits. The first of these devices was a

spatial harmonic type TW tube described by Chodorow and Nalos,¹¹ which gave in excess of 300 kw of pulsed power at S-band over a 10 per cent bandwidth (Figure 4). After the successful demonstration of the feasibility of this type of device, a great deal of interest was stimulated in a number of industrial and research institutions, leading to a wider exploitation of the periodically loaded waveguide as a slow-wave circuit. Both forward-wave circuits and spatial harmonic circuits were evolved and tried with the object of improving impedance and bandwidth. A comprehensive analysis of periodically loaded waveguide circuits for high voltage applications has been made by Craig,¹² pointing out the relative advantages of several classes of circuits. The selection of the circuit depends to a great degree on the desired voltage of operation and the desired bandwidth. Spatial harmonic circuits are usually characterized by relatively long field-free drift-spaces designed to hide the beam during periods at which it would be decelerated by the field, whereas the fundamental forward-wave circuits need not employ such drift tubes because the main component of the field is in synchronism with the beam. The energy stored per unit length, W , for a given amount of useful r-f field E , is given by

$$\frac{E^2}{W} = \left(\frac{E^2}{2\beta^2 P} \right) 2v_g \beta^2 \sim K v_g$$

It is thus proportional to the r-f impedance K and the group velocity, v_g . For a typical set of parameters suitable for fundamental and spatial harmonic interaction, using a solid beam, a comparison of the energy storage factors at

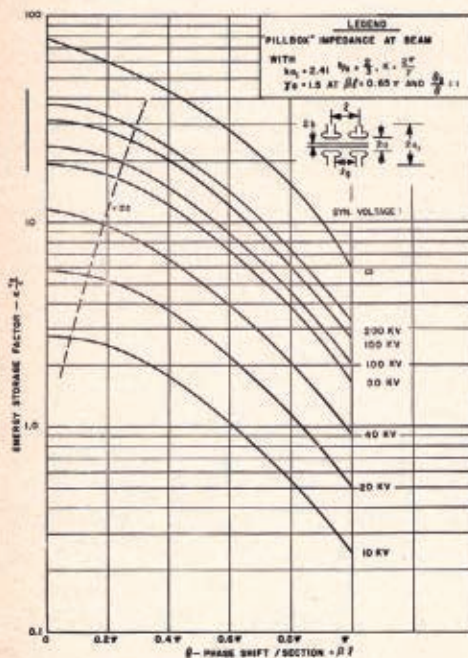


Figure 5a—Calculated energy storage factors: fundamental interaction.

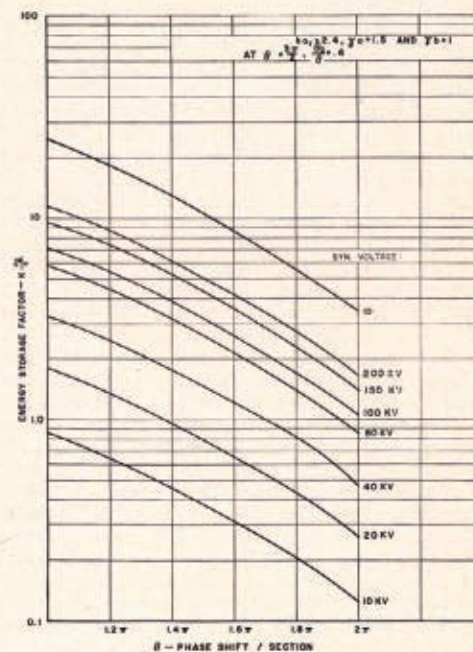
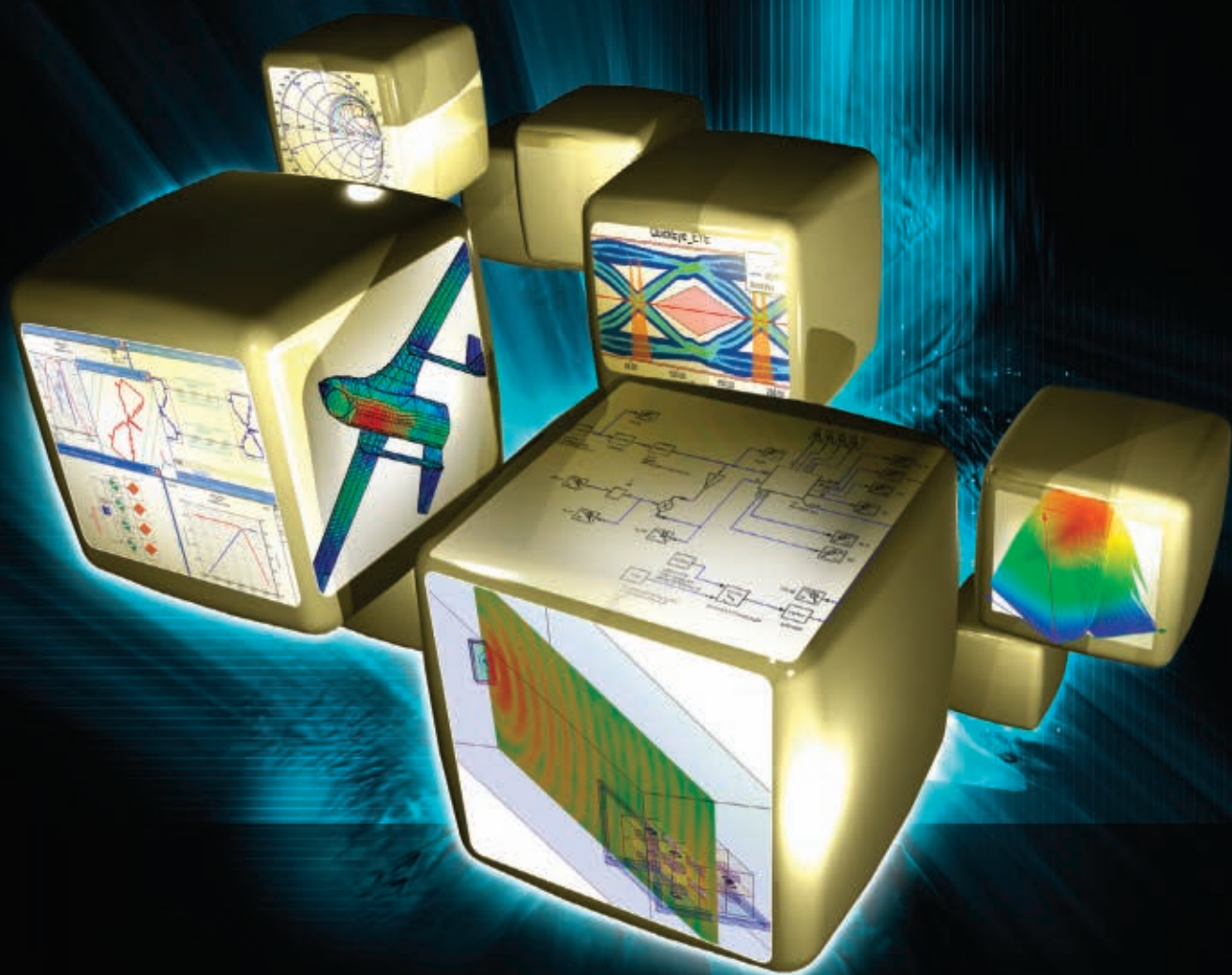


Figure 5b—Calculated energy storage factor: spatial harmonic interaction.

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various voltages is given in Figures 5A and 5B. It is seen that as far as impedance is concerned, a fundamental interaction is to be preferred.

In the following sections some applications of loaded-waveguide circuits will be described as used in present high power TW tubes, crossed-field devices and devices used for generation of high frequency waves. It will be seen that a wide range of both forward-wave and backward-wave circuits has been employed, depending not only on bandwidth and impedance considerations but also on adaptability to manufacture and compact focusing.

B. Circuits for High Power "O" Type TW Tubes

Both fundamental and spatial harmonic interaction has been employed for this application. Some circuits have employed a perturbation of the basic waveguide TM_{01} mode, whereas others have used a coaxial mode perturbed by the waveguide wall. It is possible to regard the field configurations of the slow-wave circuits as derived from several different basic transmission-line modes; the view presented here is one of convenience and usefulness to the author but is by no means the only one.

1. FUNDAMENTAL FORWARD-WAVE CIRCUITS

Two types of forward-wave circuits will be discussed; one where capacitive coupling is obtained by means of an aperture near the axis of the circuit where strong electric fields exist, and the other, where negative inductive coupling is obtained by means of special slots in the region of the magnetic field.

a. Capacitively Coupled Circuits

Some typical fundamental forward-wave circuits are shown in Figure 6. The size of the capacitive aperture determines the bandwidth and the limitation of the circuit, Figure 6A, is given by the maximum size aperture allowed to obtain good r-f coupling to the beam. Obviously, if a hollow beam of adequate power capability can be employed, this limitation is removed because

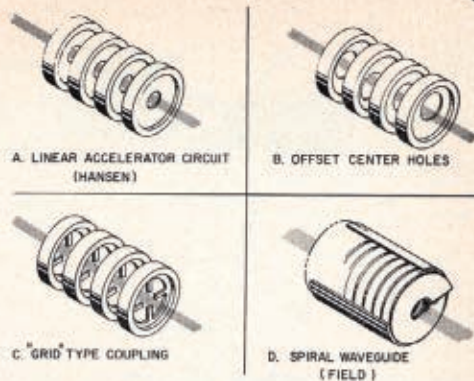


Figure 6—Some fundamental forward-wave circuits (capacitive coupling).

good r-f coupling can be maintained regardless of aperture size. Some methods to overcome this limitation are suggested in Figures 6B and 6C, where the coupling to the beam is achieved by grid-like vanes, or offset coupling holes.

b. Reversed-Loop Coupled Circuits

By means of a novel type of coupling, suggested by Chodorow and Craig,¹² it is possible to increase the bandwidth of the circuit with a fixed size center aperture using reversed loops, illustrated in Figure 7A. This type of coupling provides a microwave equivalent of a negative mutual inductance (i.e., a reactance of the same sign as that due to capacitive coupling) and has been successfully evolved at Stanford into slow-wave circuits of the "cloverleaf" type¹² and the "centipede" type¹³ shown in Figures 7B and 7C.

A TW tube of the cloverleaf type which has given 2 megawatts of peak power at S-band over a 10 per cent frequency band is shown in Figure 8. Tubes of a similar type have been built at SERL (England), General Electric Microwave Laboratory, and Varian Associates.

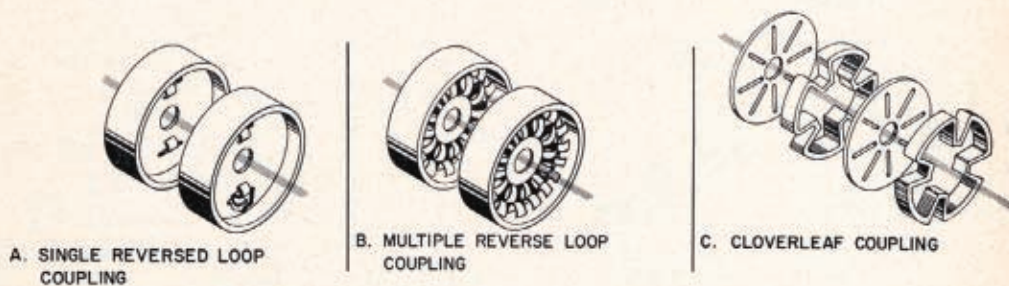


Figure 7—Circuits with negative inductive coupling (Craig, Chodorow).

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TRAVELLING WAVE TUBES: MODERN DEVICES AND CONTEMPORARY APPLICATIONS



From its conception in 1943 by Dr. Rudolf Kompfner in England,¹ and later its development by Kompfner and John R. Pierce at the Bell Laboratories in the United States,² the travelling wave tube (TWT) has become the microwave amplifier of choice for many commercial and military systems. Originally developed for communication, these devices have become fundamental to many military applications, including radar, electronic counter measures (ECM) and electronic warfare (EW) systems.

In simple terms all types of TWTs consist of an electron gun, a slow wave structure, magnetic focussing system, RF input and output couplers, and a collector. With operating voltages applied, the electron gun (containing an emitter) produces an electron beam, which is injected into the slow wave structure (SWS). The magnetic focussing system constrains the electron beam, allowing it to travel longitudinally down the centre of the slow wave structure.

RF power of the appropriate frequency is injected through the input coupler onto the slow wave structure. The electron beam and the RF signal travel down the structure at sim-

ilar speeds and an interaction between the two results in an energy transfer from the electron beam into the electromagnetic wave, thus achieving an amplification in the RF signal. The collector at the opposite end of the device to the electron gun is designed to collect the spent electron beam and dissipate the remaining energy efficiently.

TWT TECHNOLOGY

Developments in material and manufacturing technologies over the past 50 years have aided the advancement of TWT capabilities. Improvements in high purity vacuum-compatible materials such as nickel/copper alloys and pure oxygen-free, high-conductivity (OFHC) copper have been a major contributor to improvements in both life and reliability.

Advances in thermionic cathode technology, resulting in increased operating life, and the development of high-energy product mag-

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netic materials such as Samarium Cobalt, have enabled the reduction in size of magnetic circuits. The use of computer controlled processing systems and component-manufacturing machines have seen achievable tolerances reduce by an order of magnitude, along with a considerable reduction in unit cost.

Numerous structure designs have been conceived since its original conception, offering various advantages to different applications. Ervin Nalos's paper, first published in the December 1959 issue of *Microwave Journal* (reprinted this month), focused primarily on high power travelling wave tubes.³ Other circuit types

were discussed, including the simple helix, ring-bar and bifilar, demonstrating the considerable understanding and capability of different slow wave structures 50 years ago.

The major constraints to higher performance were materials technology, processing techniques and manufacturing capabilities. The 1959 paper discusses the simple helix, having the capability of continuous wave (CW) powers as high as 10 W at X-band. Today CW helix TWTs have achieved output power levels of several kilowatts at X-band, a considerable achievement, largely due to current material technologies and automated manufacturing processes.

THE HELIX

The 'simple' helix continues to be the most commonly used SWS in TWTs since its inception by Kompfner. In its simplest form, a wire or tape wound in the form of a helix, it exhibits the greatest potential of all SWSs, in terms of dispersion control and thus greatest operating bandwidth. Performance characteristics can be controlled through the design of simple and complex pitch tapering, to enhance both narrow and broadband operation, optimising gain, power and efficiency. **Figure 1** shows both a sketch of a simple helix structure and a photograph of a tungsten tape helix.

Dispersion characteristics can be controlled through design of helix supports, in terms of material choice and cross-sectional shape and electrically conductive dispersive vanes. Vanes offer the greatest opportunity for dispersion control and are commonly utilized within broadband TWTs of greater than an octave bandwidth.

BIFILAR CONTRA-WOUND AND RING-BAR TWTs

Variants on the simple helix include the bifilar helix (made up of two contra-wound helices of equal but reversed pitch), the ring-bar and the ring-loop structure. Sketches of both bifilar and ring-bar structures can be seen in **Figure 2**. These types of structures enable higher power handling through both thermal capability and higher voltage operation without giving rise to backward wave oscillation (BWO), a major constraint in simple helix structures. The downsides to these types of structures (in relation to

the simple helix) are the limitation of bandwidth due to the high dispersion characteristics of the SWS and the increased complexity in manufacture, which directly impacts the cost.

COUPLED CAVITY TWTs

The feature that distinguishes the coupled cavity TWT from other types is the SWS, which consists of a series of cavities, is coupled by slots. The benefits of this are that the cavities can be designed to operate with high voltage electron beams enabling peak output powers of 10s to 100s of kilowatts, with high average powers.

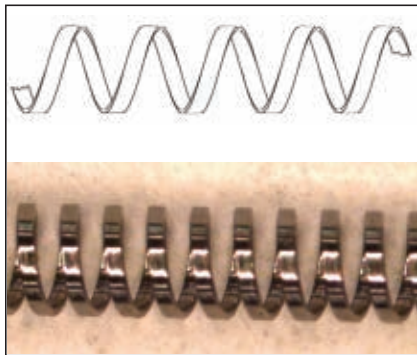
The space harmonic coupled cavity circuit, favoured by most users because of the high (up to 20 percent) instantaneous bandwidth achievable, is particularly suited to integration of periodic permanent magnetic (PPM) focussing. The result is a very compact device that is used in mobile radar systems. Very high average power and CW coupled cavity TWTs are available but these utilise solenoid focussing, which requires significant electrical power and weighs more than PPM focussed devices. **Figure 3** shows two of the more commonly used coupled cavity type structures: slotted and clover-leaf.

CATHODE TECHNOLOGY

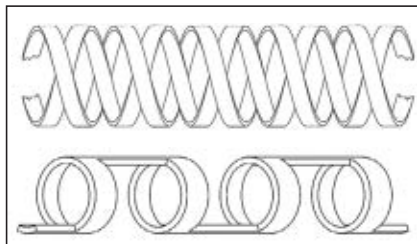
Developments in the field of emitters, the electron source of travelling wave tubes, have enabled the development of devices capable of 10s and even 100s of thousands of hours of life. Fifty years ago the electron sources used in vacuum devices, including the early TWTs, would have been of the oxide-coated type emitter, restricted to pulsed or low current density CW applications, ideally suited to high-power pulsed devices, like the coupled cavity TWT, used for radar-type applications.

Today, with advances in cathode technology, materials and processing, a range of impregnated tungsten matrix cathodes are the cathode of choice. Capable of considerably higher mean currents, operating CW at high current densities ($> 20 \text{ A/cm}^2$), the coated tungsten matrix (M-type) cathode is the most commonly used.

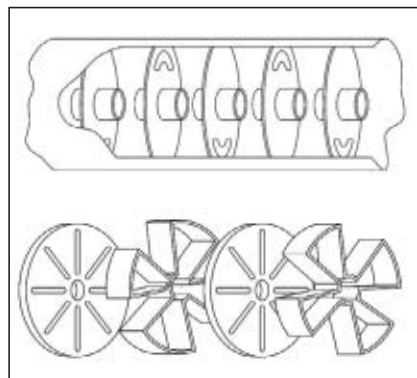
Other advantages over the oxide cathode include higher resistance to poisoning, increased life and improved manufacturing tolerances be-



▲ Fig. 1 Simple helix slow wave structure (top) and photograph of a tungsten helix structure (bottom).



▲ Fig. 2 Bifilar contra-wound (top) and ring-bar (bottom) slow wave structures.



▲ Fig. 3 Slotted (top) and clover-leaf (bottom) coupled cavity slow wave structures.

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cause of the machined emitting surface. In addition to this, coupled with a potted heater assembly, cathodes have been manufactured to survive and function under the most severe vibration and shock levels.

Work continues towards making advances in cathode design and manufacture. Developments include mixed-matrix and reservoir cathodes, and more recently the field emitting cold cathode.⁴ Although in its infancy,

recent research has produced samples nearing the capabilities required for a TWT electron source.

TWT DESIGN AND VALIDATION

The introduction of computer modelling and its advances over the past three decades have had a marked impact on the vacuum electronics industry, taking design from long-hand calculations (sometimes only comprehensible to the most ad-

vanced mathematicians) to user-friendly computer simulation of all aspects (electronic, mechanical, thermal) of the device design.

3-D electron beam simulation programmes enable accurate simulation of beam entry, focussing systems and collection. **Figure 4** shows a plot from an electron gun model, using OPERA 2D. Together with the constant advances in computing power, designs can be realised in hours or even minutes, and once validated, the latest software is capable of previously unprecedented levels of accuracy.

Advances in Particle in Cell (PIC) and parametric codes, combined with complex optimisers, enables accurate simulation of the interaction between electron beam and the slow wave structure. Increases in computing power have enabled the simulation of complex slow wave structures and complete RF circuits. **Figure 5** is a cross-section of a helix SWS, showing dielectric helix support rods and dispersion vanes, typically used in broadband helix TWTs.

In addition to the advances in electrical design enabled by new codes and improved processing speeds, commercially available codes can be utilised for thermal and mechanical stress analysis. Thermal analysis of TWT collectors enables improved thermal management of new designs. **Figure 6** shows a simple thermal model of a single stage collector. The modern-day designer

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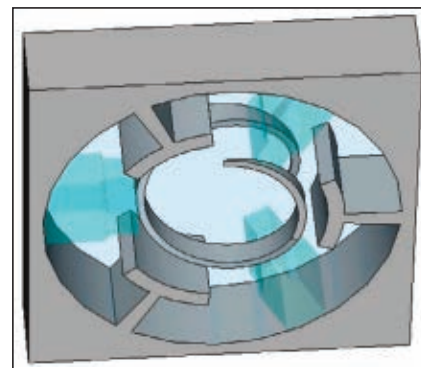
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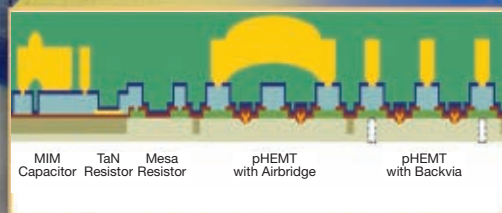
▲ Fig. 4 OPERA 2D finite element software—electron gun model.



▲ Fig. 5 Microwave Studio parametric model of a helix SWS.

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Ron	1.2 Ohm-mm
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* f=10 GHz, Vdg=7 V, Ids=160 mA/mm

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now has a complete package of modelling and simulation codes that, when fully validated with real device data, enable a right-first-time design approach significantly reducing development times and costs.

PRESENT STATE OF THE TWT ART

TWT production is limited to a handful of manufacturers throughout the world; major suppliers include CPI, L-3 and Teledyne in the US, e2v,

Thales and TMD in Europe, NEC in Japan, and several developing manufacturers in both India and China.

Determining the current state of the art is difficult; many government-funded programmes restrict the publication of data and commercial confidentiality is high due to the competitive markets. **Table 1** shows a cross-section of products from various manufacturers, giving a broad view of current capabilities.

HELIX TWTS

Satellite Communications (Ground-based)

Low cost, high reliability and high linearity are key in this commercially competitive market. Offerings are available from all the major manufacturers, whether it is earth stations, Satellite News Gathering (SNG) mobile systems, network hubs or small lightweight flyaway pack systems. Demands for bandwidth are forcing the move towards higher frequencies (Ka-band) and the onset of digital broadcasting requires higher powers.

Notable performance advances have been achieved by NEC and L-3 in the development of Ka-band helix TWTs for this market, with CW power levels as high as 500 W. Another growth area is in small lightweight amplifiers used in flyaway and hand portable systems. Reductions in luggage weight, by most airlines around the world, has forced demand for these systems to become smaller and lighter. In a market where solid state amplifiers and travelling wave tube amplifiers (TWTAs) compete head to head, e2v has launched a range of TWTAs (StellarMini™) that are the smallest and lightest currently available.

Advances in multi-octave TWTs developed originally for military applications has led to opportunities in multi-band TWTAs for both commercial and military communications. Dual- and tri-band devices have been developed by Teledyne, CPI and e2v.

Satellite Communications (Space)

Key attributes of the space TWT include long life (mission life greater than 20 years), high reliability, low power consumption (high efficiency) and low mass. The majority of all TWTs in space have been manufactured by Thales (France) or L-3 Electron Technologies Inc. (US; formerly Boeing/Hughes) with developments progressing at CEERI (India).

Future demand is moving up in frequency as advances in solid state technology capture the low frequency end of the operating spectrum (up to Ku-band) and the overcrowding of traditional bands forces the need for greater bandwidth utilization. The number of satellites being launched at Ka-band is growing fast and is set to continue.

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* US Patent 6,414,563

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TABLE I

GLOBAL SELECTION OF CURRENT HELIX AND COUPLED CAVITY TWTs

Market	Product	Manufacturer	Frequency/ Band (GHz)	Output Power (W)
Satellite Comms (Ground)	TH3977 ^[5]	THALES	Ku	750
	VTU-6397H1 ^[6]	CPI	Ku	1200 (Peak)/ 600 (CW)
	MTG5338X ^[7]	TELEDYNE MEC	C/X/Ku	350/600/350
	LD7314 ^[8]	NEC	Ka	350 (Peak)/ 250 (CW)
Satellite Comms (Space)	9100HR ^[9]	L-3	K	50 to 130
	TH4725B ^[5]	THALES	Ku	100 to 150
	TH4626 ^[5]	THALES	Ka	30 to 60
	VTS5754F ^[6]	CPI	S Duty	130K, 8%
Radar	N10570A ^[10]	e2v	X	20K, 8% Duty
	TL35038 ^[5]	THALES	Ka	1K, 12% Duty
	L6049 ^[11]	L-3	4.5 to 18	110
ECM/EW	N20160 ^[10]	e2v	4.5 to 18	50
	TH3893 ^[5]	THALES	6 to 16	1500

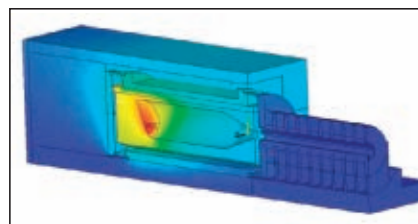
Radar

Traditionally the realm of high peak power helix and coupled cavity TWTs, the development of active phased-array radar has seen a significant shift away from vacuum devices towards solid state technology, more suited to compact packaging required in an array system. Although as requirements become more demanding, requiring higher efficiency, lower thermal dissipation and greater reliability, customers of microwave amplifiers are turning back to TWTs as the preferred option. Over the past three decades TWT reliability has increased considerably; space TWTs have achieved MTBFs of six million hours with efficiencies reaching 50 percent, which makes the TWT a viable alternative to solid-state amplifiers (SSA). Advances in mini TWT technology, driven by airborne towed decoys and MPMs, has led to compact high efficiency devices ideally suited to phased-array and Synthetic Aperture Radar (SAR) applications.

ECM and EW

The largest market for the helix TWT is in ECM and EW applications, which has seen tens of thousands of devices built into expendable

decoy systems and ECM pods around the world. The demands on devices tend to be a combination of those for all other applications, with the added complexity of operation over multi-octave bandwidths. Current demands are for greater bandwidth and higher efficiency in smaller lighter weight packages that are able to operate over extreme temperature ranges and high altitudes. With the growth of unmanned air vehicle (UAV) applications, the military business for TWTs continues to grow.



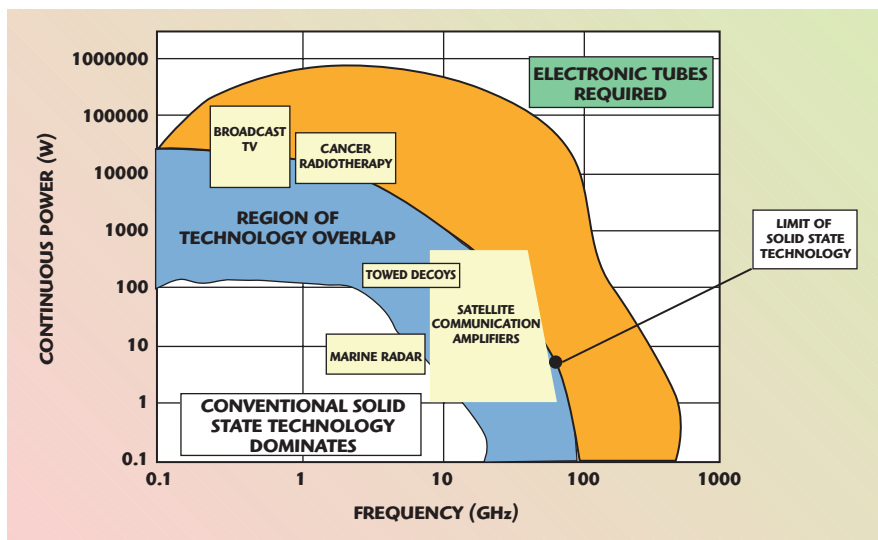
▲ Fig. 6 3D thermal simulation model of TWT collector assembly.



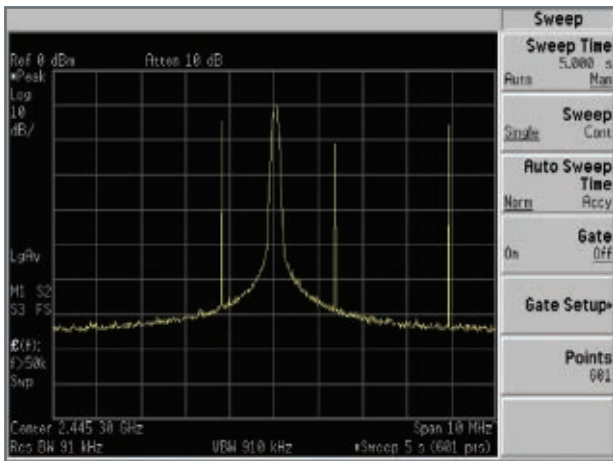
▲ Fig. 7 Deployed fibre optic towed decoy.

Over the past decade, the likes of L-3, CPI, Thales and e2v have developed ranges of mini TWTs, predominantly for airborne applications with bandwidths of greater than 2 octaves covering 4.5 to 18 GHz and power levels now exceeding 100 W CW across the full band. Devices have been proven to survive and operate at temperatures ranging from -55° to $> 150^{\circ}\text{C}$, altitude > 70 kft and shock levels in excess of 500 G.

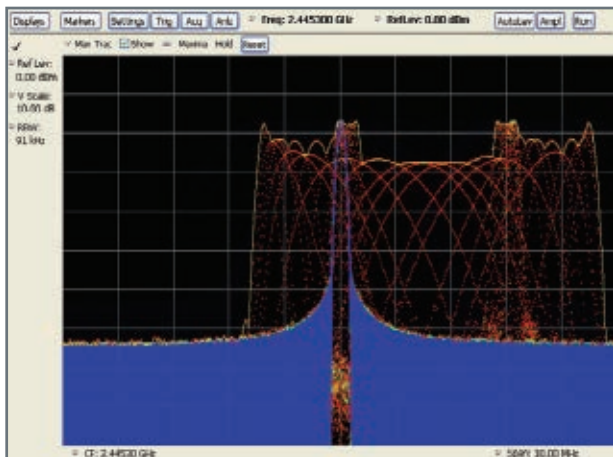
Utilization of multi-stage depressed collectors has seen mid-band efficiencies top 50 percent, resulting in reduced thermal footprints and prime power requirements. CPI¹² has, over the past two decades, delivered many thousands of mini TWTs into the Raytheon¹² Goleta ALE-50 towed decoy programme, which is a notable



▲ Fig. 8 Frequency and power capabilities of present amplifier technologies.



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5 seconds



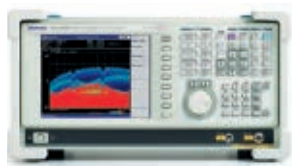
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achievement. **Figure 7** shows a typical fibre optic towed decoy (FOTD) TWT platform being deployed.

Advances continue to be made at higher frequencies covering the 18 to 40 GHz band for countering and jamming new threats. With continually changing and advancing threats, plus the upgrades to existing systems, demands on the microwave amplifiers in this market are increasing, continuing to enhance efficiency and expand

bandwidth will be necessary to keep ahead of the advancing SSA sector and meet the expectations of customers.

STATUS OF COUPLED CAVITY TWTs

Many modern radar systems, including new developments, continue to use coupled cavity TWTs. This is because, contrary to popular opinion, coupled cavity TWTs are often more robust, long-lived, reliable and effi-

cient than the solid state alternative. Coupled cavity TWTs currently manufactured cover the frequency ranges from D-band up to M-band. Instantaneous bandwidth of 10 percent is required for most applications, but various techniques have been employed to increase this to 20 percent (normally compromising efficiency or power considerations).

The conventional manufacturing technique for coupled cavity TWTs employs individual cavities and coupling plates brazed together. At Ka-band and above, this technique becomes very expensive, as the machining tolerances become extremely tight.

Alternative methods of production for high frequency TWTs have been investigated, with the ladder structure used by CPI being the most popular. Modern computer aided design techniques have been used to redesign existing coupled cavity TWT designs; the result of this has been much higher manufacturing reproducibility, and hence yields.¹³

New radar transmitter specifications continue to demand more from the TWT designer; the areas of particular interest are higher mean power, faster warm-up time and higher efficiency. The use of computer aided design tools to investigate these areas has been successfully employed. Notably, e2v has developed and built RF circuits for high mean power that overcome the natural limitation of heat being conducted through iron pole pieces.¹⁴ Other manufacturers have increased mean power by improving the electron beam confinement under RF conditions. There is no reason why both techniques cannot be combined to produce coupled cavity TWTs of higher mean power capability.

FUTURE DEVELOPMENTS

With the recent development of compound semiconductors into the power amplification domain, a number of power applications have now migrated from tube-based to solid state amplification. This is especially true of sub-kilowatt, narrow-band requirements, with recent developments in Silicon Carbide (SiC) and Gallium Nitride (GaN) extending these devices into multiple-kilowatt capability, to frequencies around 10 GHz and above.¹⁵ **Figure 8** shows the current solid-state



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and vacuum tube landscape, with respect to frequency and power.

As solid-state devices increase in capability, more applications will migrate from a tube to a transistor embodiment. However, for the present it is clear that travelling wave tubes continue to offer a compact and efficient amplifier solution, particularly under harsh operating environments. TWT amplifiers can also span a broad frequency bandwidth,

approaching three octaves of coverage from a single tube.

FUTURE DIRECTION FOR TWTs

The future remains bright for TWTs, albeit in a tougher and more competitive market place. The continued progress of solid-state amplifiers will eat into the edges of the TWT domain, but there will remain to be requirements for the amplification of microwaves beyond the present capabilities of solid-state.

For systems with limitations on size, weight, power dissipation and consumption, there are, and will continue to be, numerous applications for vacuum electronic devices (VED). Higher power levels and higher frequencies are areas where tubes have no equal. The continued advances in VED technology will sustain growth.

In the commercial market, High Definition Television (HDTV) and the onset of the digital age are demanding higher powers and higher frequencies. These are major opportunity areas for the TWT.

The defence business worldwide continues to grow, upgrades to existing systems and new platforms, such as UAVs, require higher efficiencies, smaller lighter payload packages and improved reliability. Higher definition radar systems such as SARs and phased-array radar offer opportunities for small, lightweight, high-efficiency devices.

Also, government and defence funding is being made available to the industry to continue developing products for the future. An area of considerable interest at present is in the terahertz and sub mm-wave frequency regimes. Research and development in this area include CAD design of MEMS type structures, manufacturability, detection techniques and prototype manufacture. Programmes are as yet undefined but potential uses include UAV SAR for tactical targeting and terrain avoidance and security imaging.¹⁶ ■

ACKNOWLEDGMENTS

Inputs on TWT product history and technology development have been provided by Alan Griggs (e2v principal TWT engineer) and Ian Milsom (e2v cathode development and test manager). The overview of current power amplifier technology was compiled by Dr. Cliff Weatherup (e2v strategic technology manager) and Dr. Trevor Cross (e2v chief technology officer). Product and application photographs were provided by Andy Bennett (e2v marketing).

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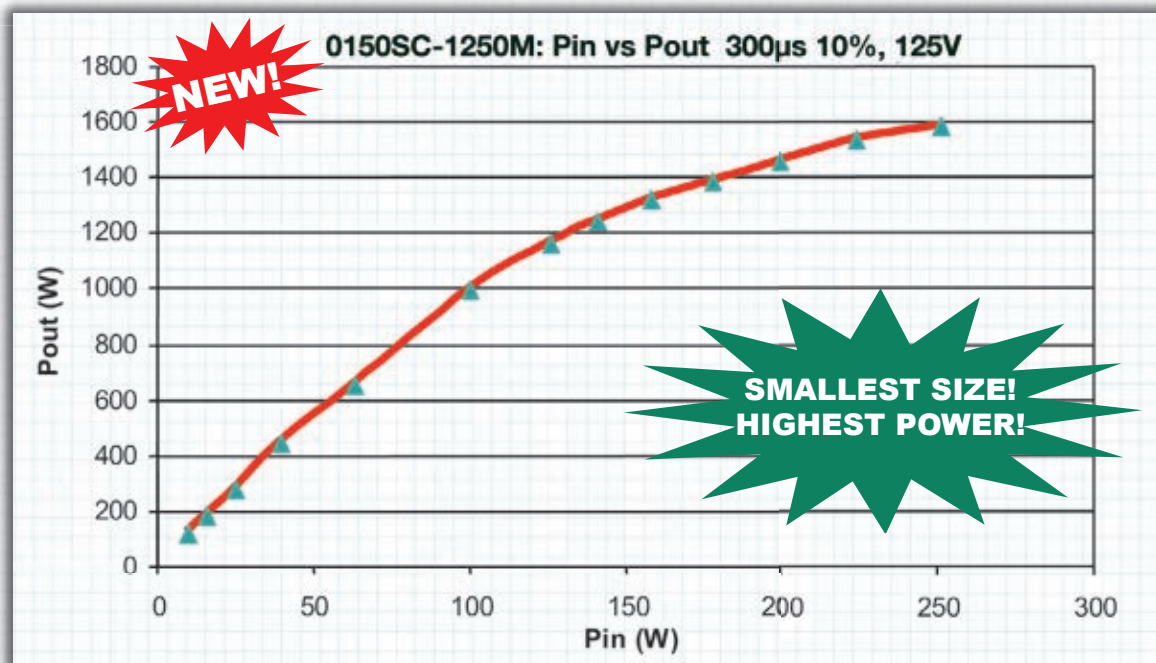
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Brian Coaker joined the English Electric Valve Co. (a GEC subsidiary, later known as EEV, now e2v technologies), Lincoln, UK, as an Apprentice Technician Engineer. He then read BEng Physical Electronic Engineering at Lancaster

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Tony Challis joined the English Electric Valve Co., Chelmsford, UK, as an Apprentice Technician Engineer in 1983. He received his HNC in electromechanical engineering from Anglia Polytechnic University (APU), Chelmsford, UK, in

1987. In 1988 he joined a team of development engineers within e2v, developing new products and re-engineering existing devices. With a strong background in mechanical engineering and experience gained in vacuum technology, he progressed to Technical Authority for Helix TWTs. Achievements in electron gun and PPM stack design led to his involvement in the successful development of a range of mini TWTs designed for airborne decoy applications. With this knowledge of TWT design and manufacture, allied with an appreciation for the vacuum electronics business, he is currently product manager for TWTs and microwave amplifier systems.

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AML48L3001	4.0 – 8.0	30	±1.0	1.2	+10	1.8:1	150
AML412L3002	4.0 – 12.0	30	±1.5	1.5	+10	1.8:1	150
AML218L0901	2.0 – 18.0	9	±1.0	2.2	+5	2.5:1	60
AML0518L1601-LN	0.5 – 18.0	16	±1.0	2.7	+8	2.2:1	100
AML0126L2202	0.1 – 26.5	22	±2.25	3.5*	+8	2.2:1	170
AML1226L3301	12.0 – 26.5	33	±2.0	2.8	+8	2.5:1	200

Broadband Medium Power Amplifiers

AML0016P2001	0.01 – 6.0	21	±1.25	3.2*	+23*	2.0:1	480
AML26P3001-2W	2.0 – 6.0	28	±2.5	6	+33	1.8:1	1500
AML28P3002-2W	2.0 – 8.0	30	±2.0	5.5	+33	2.0:1	2000
AML218P3203	2.0 – 18.0	32	±2.5	4	+25	2.0:1	450
AML618P3502-2W	6.0 – 18.0	35	±2.5	4	+33	2.0:1	1850

Narrow Band Low Noise Amplifiers

AML23L2801	2.8 – 3.1	28	±0.75	0.7	+10	1.8:1	150
AML1414L2401	14.0 – 14.5	24	±0.75	1.5	+10	1.5:1	130
AML1718L2401	17.0 – 18.0	24	±0.75	1.6	+10	1.8:1	150

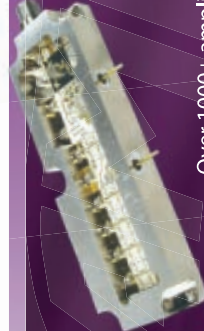
Low Phase Noise Amplifiers

Part Number	Frequency (GHz)	Gain (dB)	Output Power (dBm)	100Hz	1KHz	10KHz	100KHz
AML811PN0908	8.5 – 11.0	9	17	-154	-159	-167	-170
AML811PN1808	8.5 – 11.0	18	18	-152.5	-157.5	-165.5	-168
AML811PN1508	8.5 – 11.0	15	28	-145.5	-153.5	-158.5	-164.5
AML26PN0904	2.0 – 6.0	9	20	-150	-165	-165	-178
AML26PN1201	2.0 – 6.0	11	15	-155	-160	-160	-175

High Dynamic Range Amplifiers

Part Number	Frequency (MHz)	Gain (dB)	P1dB (dBm)	OIP3 (dBm)	DC
AR01003251X	2 – 32	21	32	52	+28V @ 470mA
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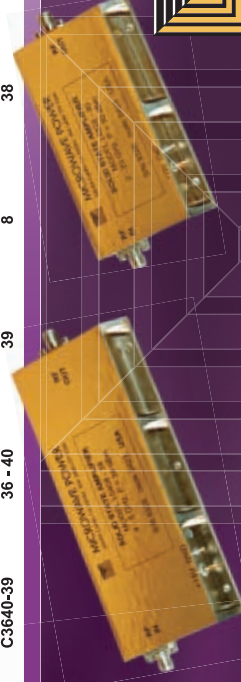
Model	Frequency (GHz)	Psat (dBm)	Psat (W)	P1dB (dBm)	Gain (dB)	DC Current(A) @ +12V or +15V
Broadband Microwave Power Amplifiers						
L0104-43	1 - 4	42.5	17.8	41.5	45	14
L0204-44	2 - 4	44	25	42.5	45	14
L0206-40	2 - 6	40	10	38.5	40	8.5
L0208-41	2 - 8	41	12	40	40	17
L0218-32	2 - 18	32	1.4	31	35	5
L0408-43	4 - 8	43	20	41.5	45	17
L0618-43	6 - 18	43	20	41.5	45	22
L0812-46	8 - 12	46	40	45	45	28

Millimeter-Wave Power Amplifiers

L1826-34	18 - 26	34	2.5	33	35	4
L1840-27	18 - 40	27	0.5	26	30	2
L2240-28	22 - 40	28.5	0.7	27	30	3
L2630-39	26 - 30	39	8.0	38	40	15
L2632-37	26 - 32	37	5.0	36	38	10
L2640-31	26 - 40	31	1.2	30	30	5
L3040-33	30 - 40	33	2.0	32	33	9
L3337-36	33 - 37	36	4.0	35	40	12
L3640-36	36 - 40	36	4.0	35	40	10

High-Power Rack Mount Amplifiers

Model	Frequency (GHz)	Psat (dBm)	Psat (W)	P1dB (dBm)	Pac (kW)	Height (in)
C071077-52	7.1 - 7.7	52.5	170	51.5	1.8	10.25
C090105-50	9 - 10.5	50	100	49	1	8.75
C140145-50	14 - 14.5	50.5	110	49.5	2	10.25
C1416-46	14 - 16	46	40	45	0.35	5.25
C1820-43	18 - 20	43	20	41.5	0.25	5.25
C2326-40	23 - 26	40	10	39	0.25	5.25
C2630-45	26 - 30	45	30	44	0.45	5.25
C3236-40	32 - 36	40	10	39	0.25	5.25
C3640-39	36 - 40	39	8	38	0.24	5.25



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Model No.	Freq (GHz)	Gain (dB) MIN	Noise Figure (dB)	Power-out @ P1dB	3rd Order ICP	VSWR
CA01-2110	0.5-1.0	28	1.0 MAX, 0.7 TYP	+10 MIN	+20 dBm	2.0:1
CA12-2110	1.0-2.0	30	1.0 MAX, 0.7 TYP	+10 MIN	+20 dBm	2.0:1
CA24-2111	2.0-4.0	29	1.1 MAX, 0.95 TYP	+10 MIN	+20 dBm	2.0:1
CA48-2111	4.0-8.0	29	1.3 MAX, 1.0 TYP	+10 MIN	+20 dBm	2.0:1
CA812-3111	8.0-12.0	27	1.6 MAX, 1.4 TYP	+10 MIN	+20 dBm	2.0:1
CA1218-4111	12.0-18.0	25	1.9 MAX, 1.7 TYP	+10 MIN	+20 dBm	2.0:1
CA1826-2110	18.0-26.5	32	3.0 MAX, 2.5 TYP	+10 MIN	+20 dBm	2.0:1

NARROW BAND LOW NOISE AND MEDIUM POWER AMPLIFIERS

CA01-2111	0.4 - 0.5	28	0.6 MAX, 0.4 TYP	+10 MIN	+20 dBm	2.0:1
CA01-2113	0.8 - 1.0	28	0.6 MAX, 0.4 TYP	+10 MIN	+20 dBm	2.0:1
CA12-3117	1.2 - 1.6	25	0.6 MAX, 0.4 TYP	+10 MIN	+20 dBm	2.0:1
CA23-3111	2.2 - 2.4	30	0.6 MAX, 0.45 TYP	+10 MIN	+20 dBm	2.0:1
CA23-3116	2.7 - 2.9	29	0.7 MAX, 0.5 TYP	+10 MIN	+20 dBm	2.0:1
CA34-2110	3.7 - 4.2	28	1.0 MAX, 0.5 TYP	+10 MIN	+20 dBm	2.0:1
CA56-3110	5.4 - 5.9	40	1.0 MAX, 0.5 TYP	+10 MIN	+20 dBm	2.0:1
CA78-4110	7.25 - 7.75	32	1.2 MAX, 1.0 TYP	+10 MIN	+20 dBm	2.0:1
CA910-3110	9.0 - 10.6	25	1.4 MAX, 1.2 TYP	+10 MIN	+20 dBm	2.0:1
CA1315-3110	13.75 - 15.4	25	1.6 MAX, 1.4 TYP	+10 MIN	+20 dBm	2.0:1
CA12-3114	1.35 - 1.85	30	4.0 MAX, 3.0 TYP	+33 MIN	+41 dBm	2.0:1
CA34-6116	3.1 - 3.5	40	4.5 MAX, 3.5 TYP	+35 MIN	+43 dBm	2.0:1
CA56-5114	5.9 - 6.4	30	5.0 MAX, 4.0 TYP	+30 MIN	+40 dBm	2.0:1
CA812-6115	8.0 - 12.0	30	4.5 MAX, 3.5 TYP	+30 MIN	+40 dBm	2.0:1
CA812-6116	8.0 - 12.0	30	5.0 MAX, 4.0 TYP	+33 MIN	+41 dBm	2.0:1
CA1213-7110	12.2 - 13.25	28	6.0 MAX, 5.5 TYP	+33 MIN	+42 dBm	2.0:1
CA1415-7110	14.0 - 15.0	30	5.0 MAX, 4.0 TYP	+30 MIN	+40 dBm	2.0:1
CA1722-4110	17.0 - 22.0	25	3.5 MAX, 2.8 TYP	+21 MIN	+31 dBm	2.0:1

ULTRA-BROADBAND & MULTI-OCTAVE BAND AMPLIFIERS

Model No.	Freq (GHz)	Gain (dB) MIN	Noise Figure (dB)	Power-out @ P1dB	3rd Order ICP	VSWR
CA0102-3111	0.1-2.0	28	1.6 Max, 1.2 TYP	+10 MIN	+20 dBm	2.0:1
CA0106-3111	0.1-6.0	28	1.9 Max, 1.5 TYP	+10 MIN	+20 dBm	2.0:1
CA0108-3110	0.1-8.0	26	2.2 Max, 1.8 TYP	+10 MIN	+20 dBm	2.0:1
CA0108-4112	0.1-8.0	32	3.0 MAX, 1.8 TYP	+22 MIN	+32 dBm	2.0:1
CA02-3112	0.5-2.0	36	4.5 MAX, 2.5 TYP	+30 MIN	+40 dBm	2.0:1
CA26-3110	2.0-6.0	26	2.0 MAX, 1.5 TYP	+10 MIN	+20 dBm	2.0:1
CA26-4114	2.0-6.0	22	5.0 MAX, 3.5 TYP	+30 MIN	+40 dBm	2.0:1
CA618-4112	6.0-18.0	25	5.0 MAX, 3.5 TYP	+23 MIN	+33 dBm	2.0:1
CA618-6114	6.0-18.0	35	5.0 MAX, 3.5 TYP	+30 MIN	+40 dBm	2.0:1
CA218-4116	2.0-18.0	30	3.5 MAX, 2.8 TYP	+10 MIN	+20 dBm	2.0:1
CA218-4110	2.0-18.0	30	5.0 MAX, 3.5 TYP	+20 MIN	+30 dBm	2.0:1
CA218-4112	2.0-18.0	29	5.0 MAX, 3.5 TYP	+24 MIN	+34 dBm	2.0:1

LIMITING AMPLIFIERS

Model No.	Freq (GHz)	Input Dynamic Range	Output Power Range Psat	Power Flatness dB	VSWR
CLA24-4001	2.0 - 4.0	-28 to +10 dBm	+7 to +11 dBm	+/- 1.5 MAX	2.0:1
CLA26-8001	2.0 - 6.0	-50 to +20 dBm	+14 to +18 dBm	+/- 1.5 MAX	2.0:1
CLA712-5001	7.0 - 12.4	-21 to +10 dBm	+14 to +19 dBm	+/- 1.5 MAX	2.0:1
CLA618-1201	6.0 - 18.0	-50 to +20 dBm	+14 to +19 dBm	+/- 1.5 MAX	2.0:1

AMPLIFIERS WITH INTEGRATED GAIN ATTENUATION

Model No.	Freq (GHz)	Gain (dB) MIN	Noise Figure (dB)	Power-out @ P1dB	Gain Attenuation Range	VSWR
CA001-2511A	0.025-0.150	21	5.0 MAX, 3.5 TYP	+12 MIN	30 dB MIN	2.0:1
CA05-3110A	0.5-5.5	23	2.5 MAX, 1.5 TYP	+18 MIN	20 dB MIN	2.0:1
CA56-3110A	5.85-6.425	28	2.5 MAX, 1.5 TYP	+16 MIN	22 dB MIN	1.8:1
CA612-4110A	6.0-12.0	24	2.5 MAX, 1.5 TYP	+12 MIN	15 dB MIN	1.9:1
CA1315-4110A	13.75-15.4	25	2.2 MAX, 1.6 TYP	+16 MIN	20 dB MIN	1.8:1
CA1518-4110A	15.0-18.0	30	3.0 MAX, 2.0 TYP	+18 MIN	20 dB MIN	1.85:1

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CA001-2211	0.04-0.15	24	3.5 MAX, 2.2 TYP	+13 MIN	+23 dBm	2.0:1
CA001-2215	0.04-0.15	23	4.0 MAX, 2.2 TYP	+23 MIN	+33 dBm	2.0:1
CA001-3113	0.01-1.0	28	4.0 MAX, 2.8 TYP	+17 MIN	+27 dBm	2.0:1
CA002-3114	0.01-2.0	27	4.0 MAX, 2.8 TYP	+20 MIN	+30 dBm	2.0:1
CA003-3116	0.01-3.0	18	4.0 MAX, 2.8 TYP	+25 MIN	+35 dBm	2.0:1
CA004-3112	0.01-4.0	32	4.0 MAX, 2.8 TYP	+15 MIN	+25 dBm	2.0:1

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General Dynamics Awarded \$23 M for Digital Modular Radios

2010. General Dynamics C4 Systems is a business unit of General Dynamics. The software-defined DMRs communicate with Ultra-High Frequency SATCOM, Single-Channel Ground and Airborne Radio Systems (SINCGARS), Line of Sight and High Frequency radios on Navy surface and subsurface platforms. General Dynamics has delivered more than 370 DMRs for use throughout the fleet and Navy shore sites, enabling secure short-range and global communications using US military standard waveforms. "By replacing what used to be racks of radios and encryption equipment, one DMR radio represents considerable savings in size, weight and power to the Navy," said Chris Brady, vice president of Assured Communications for General Dynamics C4 Systems. "The expertise we have gained from successfully executing on the DMR is particularly relevant now as we work with Lockheed Martin in the development of the Airborne and Maritime/Fixed Station component of the Joint Tactical Radio System." In March 2008, General Dynamics received a contract to develop and integrate the maritime and fixed-site joint tactical radio capabilities and provide information assurance services for the Lockheed Martin Airborne, Maritime and Fixed Site (AMF) Joint Tactical Radio System team. General Dynamics C4 Systems delivered the first Digital Modular Radio to the Navy in 1998; it was one of the first software-defined radios to be delivered under contract to the US military. In October 2004, the radio became the first software-defined radio certified by the National Security Agency for communications up to the Top Secret level. The DMR contracting office is the Space and Naval Warfare Systems Command, working on behalf of the Program Executive Office for Command Control Communications Computers and Intelligence, San Diego, CA.

Lockheed Martin Receives \$61 M Contract for Guided MLRS Rockets

Lockheed Martin has received a \$61 M follow-on contract for Guided Multiple Launch Rocket System (GMLRS) Unitary rockets. To date, more than 850 GMLRS rockets have been fired in the Global War on Terror. Work on the contract will be performed at the company's facility in Camden, AR, and Dallas, TX. Deliveries will begin in May 2010 and conclude in July of that year. "GMLRS delivers precision when warfighters need it

General Dynamics C4 Systems has been awarded a \$23 M contract for AN/USC-61(C) Digital Modular Radios (DMR), the Navy's standard communication system for newly constructed ships and submarines. Deliveries are scheduled to begin in mid-2009 and continue through

most, especially effective in urban areas," said Lt. Col. Drew Clanton, the GMLRS product manager at the US Army's Precision Fires, Rockets and Missiles program management office in Huntsville, AL. "The system's readiness rates support the consistent quality we expect and its accuracy helps keep civilians out of harm's way."

GMLRS provides the US Army, US Marine Corps and the United Kingdom Defense Forces with a persistent, responsive, all-weather, rapidly-deployable, long-range, surface-to-surface, precision strike weapon. Reliability of US Army GMLRS missions exceeds 98 percent. "Soldiers continue to tell us how satisfied they are with GMLRS, because it is ready when it needs to be and can hit precision targets from 85 Km away, a new distance record recently recorded at tests at White Sands Missile Range," said Scott Arnold, vice president for Precision and Combat Maneuver Systems at Lockheed Martin Missiles and Fire Control. "Just as in previous orders, we are committed to delivering GMLRS to the quality and dependability on which our customers have come to rely." GMLRS is an all-weather, precision strike, artillery rocket system that achieves greater range and precision accuracy requiring fewer rockets to defeat targets and limiting collateral damage. GMLRS is a Future Force system that provides the joint warfighter with immediate precision fires to engage, destroy and deny terrain to the enemy.

Northrop Grumman Scores Success for Solid-state Laser Weapon

Northrop Grumman Corp. has set new industry records in all aspects of high-power solid-state laser production, demonstrating the readiness of these compact, portable, speed-of-light weapons to take their place on the battlefield. The company demonstrated the third critical milestone for the US military's Joint High Power Solid State Laser (JHPSSL) program, Phase 3. Operating from Northrop Grumman's one-of-a-kind laser factory, the system:

- Raised its demonstrated lethality by precisely combining two laser chains to produce a record power, 30 kW, in an excellent beam-beam quality of 2.1 times the theoretical limit.
- Operated at this performance level for more than five minutes continuously and more than 40 minutes total; and
- Achieved electrical-to-optical efficiency of greater than 19 percent.

"Our march towards providing compact, electrically powered, operationally scalable and affordable laser weapons for US military services continues to produce world-leading results," said Dan Wildt, vice president of Directed Energy Systems for Northrop Grumman's Space Technology sector. "We believe this sets a new solid-state record by simultaneously demonstrating tactically significant power and beam quality for more than five minutes," stated JHPSSL Phase 3 program manager Jay Marmo.



Just as it had in two previous milestone tests, the company's JHPSSL Phase 3 laser demonstrated its third milestone ahead of schedule. "We have achieved all our major milestones ahead of schedule as we continue to rev up the power and capability. By demonstrating our ability to combine two identical, modular laser chains into a single, high brightness beam, we have proven all aspects of our scalable design to 100 kW." The JHPSSL program is funded by the US Army Space and Missile Defense Command/Army Forces Strategic Command, Huntsville, AL; Office of the Secretary of Defense – Joint Technology Office, Albuquerque, NM; Air Force Research Laboratory, Kirkland Air Force Base, NM; and the Office of Naval Research, Arlington, VA.

Raytheon Systems Excel as LPD 20 Passes US Navy Acceptance Trials

Raytheon Co. announced satisfactory system performance on-board the USS Green Bay (LPD 20) as it completed its final acceptance trials. Raytheon Integrated Defense Systems (IDS) is the total ship electronics system integrator for the LPD 17 class of amphibious

transport dock ships. The trials, which were held at Northrop Grumman Shipbuilding facilities in New Orleans and the Gulf of Mexico, demonstrated the performance and capabilities of Raytheon systems integrated onboard, including ship control and navigation, engineering control, voice and video communications, magnetic signature control systems and the Shipboard Wide Area Network. "The completion of these acceptance trials continues our legacy of reliability and proven performance as the Mission Systems Integrator for LPD 17 and our other Navy programs," said Robert Martin, IDS vice president and deputy of Seapower Capability Systems. "This milestone is a critical step toward delivering the advanced capabilities of the LPD 17 class to the Navy and our warfighters." The acceptance trials, conducted by the US Navy's Board of Inspection and Survey, represent the final construction milestone prior to ship delivery. The assessment consists of in-port and at-sea system testing and is conducted to demonstrate vessel performance and seaworthiness to the Navy. The USS Green Bay is the fourth ship of the advanced LPG class of amphibious transport dock ships. They provide the Navy's Expeditionary Strike Group with the technology and flexibility to launch and recover amphibious landing craft, such as the Landing Craft Air Cushion, operate an array of rotary-wing aircraft, as well as transport and launch the US Marine Corps' Expeditionary Fighting Vehicle.

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Thales Alenia Space and Inmarsat Sign EuropaSat ATP

Thales Alenia Space and Inmarsat have signed an Authorization To Proceed (ATP) for the development of the EuropaSat satellite to provide mobile broadcast and two-way telecommunications services in the S-band throughout Europe.

Thales Alenia Space will commence work on the satellite design, based on its Spacebus 4000C3 platform and develop it through timely Critical Design Review to support a fully compliant application for an EC-wide S-band spectrum allocation by Inmarsat, under the recently-announced European S-band Application Process. The spacecraft will carry a payload at 2 GHz generating nine S-band user spot beams in two polarizations, using a large S-band Tx antenna of 12 m diameter.

Designed with a lifetime of 15 years, the EuropaSat satellite is expected to be launched in early 2011, in compliance with the European Selection and Authorisation Process (ESAP). The spacecraft manufacturing programme supports Inmarsat's imminent application for an award of S-band spectrum, pursuant to the ESAP, which commenced on 7 August 2008 and is subject inter alia to a successful outcome of the ESAP for Inmarsat.

ST and Ericsson Provide Platform for Joint Venture

Ericsson and STMicroelectronics have agreed to merge Ericsson Mobile Platforms and ST-NXP Wireless into a joint venture. The 50/50 joint venture will have the industry's strongest product offering in semiconductors and platforms for mobile applications and will

be an important supplier to Nokia, Samsung, Sony Ericsson, LG and Sharp. The fabless joint venture will employ almost 8,000 people with pro-forma 2007 sales of \$3.6 B. ST is expected to exercise its option to buy NXP's 20 percent of ST-NXP Wireless before the closing of the transaction.

In the joint venture, ST contributes its industry-leading multimedia and connectivity solutions as well as a complete world-class 2G/EDGE platform and strong 3G offering while Ericsson contributes its industry-leading 3G and LTE platform technology. The joint venture, staffed by proven professionals across all functional areas, is designed for long-term stability in its original structure, and is set to become an industry leader in product research, as well as design, development, and the creation of cutting-edge mobile platforms and wireless semiconductors. The joint venture will be headquartered in Geneva, Switzerland, and governance will be balanced between the companies.

Forum Adds New Members Worldwide

Eight organizations working within the advanced wireless market have recently joined the SDR Forum, bringing the total number of new members joining the Forum to 25. This growth represents a 20 percent increase in member organizations.

This rapid expansion can be attributed to the growing acceptance of software defined radio (SDR) and related technologies in the mainstream wireless markets, and the value that the SDR Forum brings to its members when operating within this dynamic environment.

The eight new member organizations demonstrate the diversity of companies involved in software defined radio development both in terms of activity and geographically with five being headquartered in the US and the other three in Europe.

They are: DRS Signal Solutions (US), a world leader in providing commercial-off-the-shelf products and custom-based SIGINT solutions; ENSTA (Paris, France), one of the top French institutes of higher education in engineering; Fraunhofer IIS (Erlangen, Germany) – as the inventor of mp3 and co-inventor of the MPEG AAC audio coding standard, the Fraunhofer IIS has achieved worldwide recognition; IMEC (Leuven, Belgium) is a world-leading independent research centre in nanoelectronics and nanotechnology; UC San Diego (US) – the California Institute for Telecommunications and Information Technology (Calit2) is a partnership of UC San Diego and UC Irvine. An area of research is software-defined radio; Reservoir Labs (US) provides leading-edge consulting and contract R&D; Xenotran (US) specializes in the analysis, design and implementation of digital communication components used in wireless communication systems; and VIP Mobile Inc. (US) provides research and development, software engineering and systems integration services.

Joint Venture to Develop UK Innovation Campus

The United Kingdom Atomic Energy Authority (UKAEA), the Science and Technology Facilities Council (STFC) and international property group, Goodman, have linked up to establish the Harwell Science and Innovation Campus in Oxfordshire, UK.

Under the agreement, UKAEA will provide land at Harwell for development and an existing business base. STFC will contribute involvement in major public sector science programmes and a proactive approach to ensuring fundamental research can be harnessed and exploited by innovators, entrepreneurs and industry. Goodman will offer market access to global businesses and expertise in



long-term property ownership, development and management, as well as providing working capital for the joint venture.

Investment at the campus will encompass fundamental scientific research and the development of property, facilities and local infrastructure. A minimum of 100,000 m² of laboratory, high technology industrial and office accommodation will be developed in the first 20-year phase of the project. Up to 5,000 high value knowledge-based jobs are also expected to be created.

Indra Leads EGNOS Satellite Navigation System Study

Indra is heading the industrial group in charge of studying the feasibility and definition of the current EGNOS satellite navigation system towards a future Multiconstellation Regional System (MRS) for the European Space Agency (ESA). The team is composed of Astrium-

EADS (Germany), Deimos Engenharia (Portugal), IN-ECO (Spain), Novatel (Canada) and the Polytechnic University of Catalonia (Spain), in addition to Indra (Spain).

The project budget is €1.5 M and the execution period is 18 months.

The EGNOS system currently provides air, sea and land information, using the North American GPS system. The objective of the study is to analyze how it should evolve so that it can take advantage of the greater number of satellites and constellations that will be in place in a few years' time, which will offer a greater volume and quality of information.

The industrial team will define the system requirements, technical specifications, design of the necessary navigation algorithms, both for the system and the end user application, features verification simulations and system architecture.

The aim is to analyze the possibility of evolving the current EGNOS system, turning it into a multiconstellation system, capable of improving regionally, within the European zone, the features offered on an individual basis by the different satellite systems separately. It will combine the signals of the future constellations of the American GPS, the Russian Glonass, the Chinese Compass/Beidou and the European Galileo systems to offer more advanced services to a greater number of users in critical, high-performance or commercial application areas. Once the study has been completed, the team will develop a preliminary prototype, based on a simulator of the various system components.

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Sensors Take the Growth Baton in the Global MEMS Market

Driven by new demand from consumer electronics and wireless applications, the global market for Microelectromechanical Systems (MEMS) will expand to \$8.8 B in 2012, up from \$6.1 B in 2006, iSuppli Corp. predicts.

"The markets for mainstay MEMS actuator prod-

ucts—like inkjet heads and Digital Light Processor (DLP) chips from Texas Instruments Inc.—finally have passed the baton to MEMS sensors to drive the next growth wave in the market," said Jeremie Bouchaud, director and principal analyst, MEMS, for iSuppli. "The new wave is partly founded in the rapid rise of consumer electronics applications such as motion sensors for gaming, laptops and digital still cameras. Mobile handsets will also be a strong area, with MEMS sensor revenue in this area to rise at a 22.9 percent Compound Annual Growth Rate (CAGR) to reach \$925 M in 2012."

Four main segments collectively will account for slightly more than 60 percent of total MEMS market revenue in 2012: consumer electronics, mobile handsets, automotive and industrial process control. Aside from the consumer and wireless applications, market pull is being exerted by the automotive sector, an established area set to receive new impetus as a result of mandates for safety and new emissions standards. Demand also will be driven by a diverse range of applications in industrial processing and control.

The one bright spot for actuators is in Radio Frequency (RF) MEMS switches used in mobile handsets and test equipment. This market will grow at an annual rate of more than 100 percent from 2006 to 2012, and will account for \$261 M in actuator revenue in 2012, up from just \$6 M in 2007.

"The consumer electronics and mobile communications fields are much more dynamic than the previous mainstay markets for MEMS," Bouchaud said. "Existing companies have a great opportunity to ride this wave and new players have a chance to address a relatively open market. However, deep R&D pockets are essential to compete in this area, and the companies that will succeed will be those that bet on and invest in building dedicated mass-production facilities." Pioneering companies with brand new MEMS products tend to enjoy a lengthy monopoly in the market, such as Texas Instruments with its DLP chip or Knowles with MEMS microphones.

Meanwhile, in fast-moving markets like consumer electronics and automotive sensors—the latter driven by mandates—economies of scale will be the norm, with sensor companies attempting to address both sectors. iSuppli also expects the pace of mergers and acquisitions to accelerate in 2008 and 2009, concentrating MEMS market share among fewer players. Please visit page 212 of this month's issue of *Microwave Journal* for more market analysis from iSuppli Corp.

Wireless USB Enters into Competitive Market

Wireless USB refers to the Certified Wireless USB (WUSB) standard based on ultrawideband (UWB) technology that is compliant with WiMedia Alliance specifications. The subject of discussion for several years, WUSB finally hit the market in 2007 in notebook PCs from Dell

and Lenovo, and in hub and dongle solutions from Belkin, IOGear and D-Link. The debut of these devices was a bit inauspicious, with relatively few devices shipping worldwide in 2007. However, the beginnings of a new wireless ecosystem have launched, and should lead to increased shipments in the years ahead.

Wireless USB is based on the same host/device architecture as wired USB, so the PC is the center of WUSB world. The Dell and Lenovo releases mark a promising start. But the question for WUSB is: Where next? In wired USB, there was a natural progression from PCs to PC peripherals to Consumer Electronics (CE) and mobile phones. However, wired USB was significantly less expensive than WUSB, which made it an easy decision to add for vendors of even the most price-sensitive PC peripheral and CE vendors. A WUSB chip solution, on the other hand, currently sells for over \$10, even in high volumes. This makes it very difficult for these same vendors to add, especially when there is no guarantee that WUSB will penetrate the vast majority of the PC market, as wired USB did. These relatively high ASPs will make WUSB adoption a relatively long-term process.

As UWB chip companies gear up production and ASPs decline, additional PC, PC peripheral and CE vendors will adopt the application. Notebook PCs will lead the adoption of WUSB. Within the PC peripheral market, there will be some interest from vendors for applications such as printers, multifunction peripherals and external hard disk drives. In the CE market, digital still cameras, digital camcorders and portable media players (PMP) should adopt WUSB in limited quantities over the next few years. However, significant WUSB adoption in these markets will not occur until WUSB chip solution ASPs come down to about half of their current levels. The competition for WUSB is fierce. It comes from other WiMedia UWB-based standards, such as Bluetooth over UWB and IP over UWB. However, the toughest competition for WUSB will come from Wi-Fi. A proven, inexpensive technology that has been through several generations, Wi-Fi is in every mobile PC shipping today, and has made inroads into many PC peripheral and CE applications, as well as into mobile phones. In addition, Intel's efforts to make Wi-Fi more Wireless PAN-friendly are directly aimed at WUSB. Ultimately though, UWB and WUSB will succeed because they solve problems that no other technology can; the ability to transmit large amounts of data over short distances from one device to another with relative power efficiency.



Online Social Networking Goes Mobile: 140 Million Users by 2013

Online social networking is huge and growing strongly, but what happens when all those virtual friends hit the road? Increasingly, they will be able to keep in touch via mobile versions of their favorite social networks, running on their cellular phones. ABI Research forecasts that in

2013, more than 140 million subscribers will share "anytime, anywhere" experiences this way, and they will generate subscription revenues in excess of \$410 M.

"Subscriber numbers for mobile social networking will climb at a relatively modest rate for the next three or four years, but will then start to accelerate sharply," says research director Michael Wolf. "That uptick is based on assumed acceptance levels in the giant emerging markets such as Brazil, Russia, India and China. Those countries are wildcards, very difficult to estimate, so we are quite conservative in our forecasts."

Some mobile versions of social networks will follow the same model common to today's Internet-based groups such as MySpace and Facebook: free browser-

based access. Such models pose a problem for mobile operators by limiting their slice of the revenue to a charge for data traffic. "The ideal scenario for the mobile operator includes a recurring revenue stream: a subscriber paying \$1.99 or \$2.99 a month to have this application on their handset," says Wolf.

Beyond the relatively modest subscription revenues that mobile social networking will generate, there will also be significant opportunities in mobile advertising as well as in mobile content sales. A recent end-user survey conducted by ABI Research showed that mobile users of social networks are likely to consume two or three times as much digital mobile content (pictures, music, videos and games) than their "asocial" peers. That would suggest a golden marketing and advertising opportunity yet, says Wolf, that is not happening: "They are not offering the right kinds of products for these users. The advertising is not that sophisticated yet. Social networking applications have to be uniquely mobile and not reliant entirely on advertising-based revenues, at least not initially."

ABI Research is a market research firm focused on the impact of emerging technologies on global consumer and business markets. For more information, visit www.abiresearch.com.

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What You Should Know About MIMO Operation and Measurement

By: **PETER CAIN**

Wireless Solution Planner, Agilent Technologies
peter_cain@agilent.com

MIMO techniques are becoming a popular combination with OFDM radio formats because they offer the possibility of increased spectral efficiency. The first commercially available MIMO system was in WLAN, but the interest has spread to cellular formats including WiMAX and LTE. Each format has adopted slightly different techniques and terminology, sometimes making it a little difficult to be sure what is being discussed.

MIMO systems also introduce a new dimension in test - that of the cross coupling of signals between hardware transmit and receive paths. This gives rise to new performance measurement techniques to augment the single channel tests that remain the starting point.

A selection from Agilent's "Ten Things You Should Know About MIMO" are presented in this paper, with the intention of giving the user an overview of the operation of MIMO technology and test methodology. Each item uses an example to highlight the impact on the radio system or associated test. A poster that summarizes all ten points is available from Agilent on request (order information can be found at the end of this paper).

The distinction between MIMO spatial multiplexing and diversity

The term "Multi-Input Multi-Output" can sometimes be applied to other multi-antenna techniques, such as transmit and receive diversity, which do not directly increase the spectral efficiency of the radio link. In practice, diversity techniques will be just as important as the spatial multiplexing that does fundamentally increase capacity, and the two methods will often be combined. This explains why we will see base stations with four antennas, even though the mobile only has two.

Referring to figure 1, the key to spatial multiplexing is the simultaneous transmission of separate portions of the incoming user data. It is inevitable there will be some cross coupling as the signals

travel through the radio channel, which includes the antennas. The art of MIMO is to avoid the transmissions simply being interference to each other. Doing this means you have to know how the radiated signals are coupled, which requires there to be as many receivers as transmitters. This leads to the first item we should know.

Spatial multiplexing requires at least two transmitters and at least two receivers. The receivers need to be in the same place.

The receivers need to be in the same place because it is the combination of the information they recover about coupling that is used to separate the data streams, or what are called codewords in 3GPP LTE.

For measurements which post-process the signals, the constraint of the receiver hardware being in the same place is removed because the measurement software, like the Agilent 89600 VSA, can combine IQ data from multiple inputs and then perform the signal separation and analysis. Another special measurement case is where the signals are connected to the analyzer with cables and never coupled, i.e. direct mapped. It is then possible to recover each codeword (stream) by connecting a single input analyzer to each transmitter in turn.

If the signal being tested remains substantially constant from frame to frame, it is also possible to capture individual signals with a single switched input. An example of equipment using this technique for WLAN is the Agilent N4011A MIMO Multi-Port Adapter.

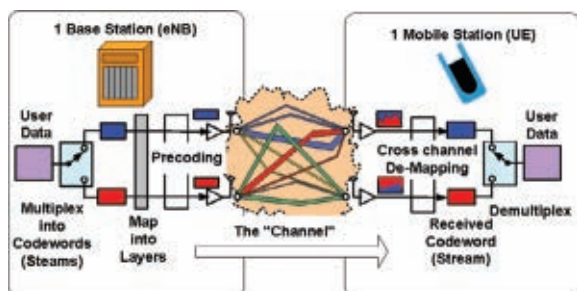


Figure 1 Cellular style asymmetric MIMO operation.

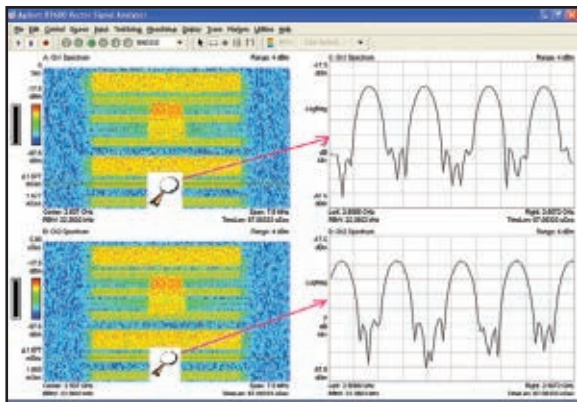


Figure 2 The distinct MIMO channel training subcarriers in LTE.

MIMO techniques are applied differently in the downlink and uplink of a cellular radio system.

In WLAN, the radio link is designed to allow symmetric operation. Figure 1 shows how this model has changed for cellular use, where the internet-led data downloading model results in the downlink being designed to have higher capacity than the uplink.

WiMAX and LTE base stations will have at least two transmitters. A number of designs have four or more transmitters, allowing the combination of MIMO and transmit diversity or phased array beamforming. All mobiles capable of supporting MIMO will have two receivers. The benefit of receive diversity is sufficient to mean mobiles would probably have two receivers even if MIMO is not initially implemented.

Figure 1 also shows the terms associated with the multiplexing of the incoming data signal into streams and layers. The incoming user data is separated into codewords (streams). If spatial multiplexing and diversity are being used in combination, there is a further step of mapping the codewords to layers, shown in the grey box. In this figure, direct mapping is shown, where no intentional cross coupling takes place before transmission.

In WLAN and WiMAX the incoming user data is multiplexed into streams which have the same modulation format (QPSK, 16QAM etc), but in LTE it is possible to have different modulation applied to each codeword. This points us to another of the MIMO fundamentals relating to the distinct difference between channel and data recovery.

MIMO signal recovery is a two-stage process.

Prior to demodulating the individual streams, the signals which were coupled as they travel through the channel have to be separated. To do this, the receivers look for channel training information which is unique to each transmitter. The generic term for a method using a special training mechanism is “non-blind”.

In WiMAX and LTE this part of the signal can be made clearly visible. Channel estimation subcarriers are split among

the different transmitters, so that no transmitter is using the same frequency at any one time. 802.11n originally considered this method, but settled on the use of orthogonal codes to distinguish the transmitters.

Figure 2 shows the spectrograms of two signals measured directly from LTE transmitters, and the zoomed-in spectral component for one of the training symbols. The LTE reference signal (RS) subcarriers can clearly be seen to be using different frequencies. Unlike the WiMAX pilots, the RS is only transmitted every 3rd or 4th symbol. The power level of all the subcarriers is the same, and their phase and timing relationship is known, which means it is possible to create a vector representation of the channel. This in turn provides the coefficients required to separate the data streams.

Phase differences don’t affect open loop MIMO.

Open loop MIMO means the transmit signals are direct mapped. No feedback from the channel is used to couple (precode) the MIMO aspect of the signals.

Another way of saying this is that phase only matters when you couple different signals twice, which is most easily explained using the coupling of two CW signals on different frequencies. The first time they are combined there may or may not be a known phase relationship between them. It doesn’t matter; the amplitude and phase of the two components will not be affected. If, however, they are coupled again, part of each signal will be common, and they will sum as vectors. The result will be changes in both amplitude and phase dependant on the combination of the original phase and the coupling factor. Complete cancellation could be one result.

This simple vector addition example explains why open loop MIMO, where the transmit signals have not been coupled, are not affected by the phase of the transmitted or received signals. The signals are only coupled once - in the channel. It also explains why uplink MIMO operation using two physically separated mobiles can work. Incidentally, precoding cannot be applied in this case, both because the input data is only available separately in each mobile, and also because the phase between mobiles cannot be controlled.

Figure 3 shows a test configuration for UL multi-user, MU, (collaborative) MIMO. The dashed line indicates the process that would take place in a real system, where the base station controls the transmission timing and power of each mobile such that the signals arrive aligned at the base station receiver. The mobiles themselves tune their frequency to match the base-station reference. In a test configuration, cables can be used and timing, power and frequency offsets can be applied with other impairments to ensure the receiver algorithms are sufficiently robust.

Cross-channel measurements can be made using a single input analyzer.

Most engineers will start with single input measurements because they are simple and provide much of the basic information about how well the components in the radio are working using available

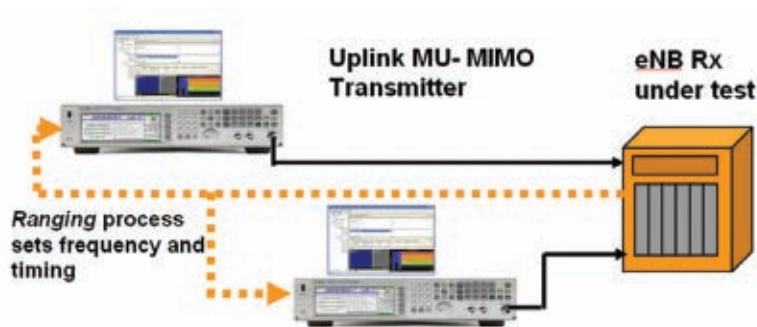


Figure 3 Operation of multi-user (collaborative) MIMO in the uplink relies on the system working with only approximate power, frequency and timing alignment. The Agilent MXG with signal studio software-based test configuration shown here allows these parameters to be varied individually.

equipment. The presence of the subcarriers used for MIMO channel training in LTE and WiMAX allows a significant extension to what can be done with a single input analyzer.

As part of the measurement demodulation process, the isolation between channels can easily be measured. This assumes the signals have not been coupled in the transmitter. In LTE, the reference signal is not precoded, so even when precoding is applied it does not affect the measurement. For WLAN and WiMAX, direct mapping should be used.

Signals using transmit diversity only require a single receiver, so they can be fully analyzed with one input. Even MIMO signals that are direct mapped can be individually analyzed, although it will not be possible to remove any unwanted coupling. The single input analyzer should be connected to each transmitter output in turn, and the analysis configured for the appropriate codeword (stream).

The most precise RF phase and timing measurements can be made with a single input analyzer. If a power combiner is used to feed multiple inputs into the single input analyzer, as shown in figure 4, relative timing and RF phase measurements may be made by demodulating the signals and comparing the symbol alignment. This method entirely removes any effect of additional equipment, and can offer sub-nanosecond and degree-measurement resolution.

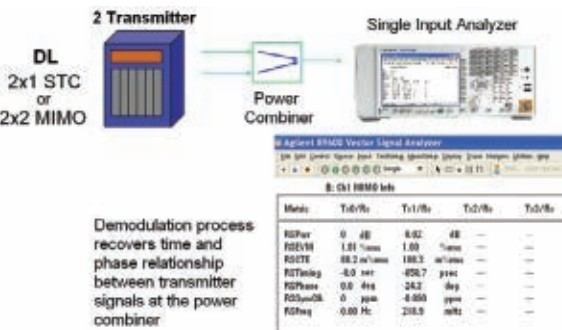


Figure 4 Cross-channel measurements using a single-input MXA spectrum analyzer and power combiner include RF frequency and phase

Antenna configuration has a major impact on the channel-path correlation.

After the receiver has been proven with static channels, fading according to different pedestrian and vehicular speed profiles can be added, using equipment such as Agilent's new PXM MIMO Receiver Tester. As noted earlier, the channel includes the antennas at both

transmitter and receiver. There has been a lot of effort to model how changes in the antenna configuration affect the path correlation.

For certification, a subset of the possible antenna configurations is chosen, but during design or more thorough performance comparisons, it is important to assess performance using a much wider range of scenarios. The Agilent PXM MIMO Receiver Tester provides the flexibility needed to do this, calculating the correlation factors as it does so.



Agilent's N5106A PXM MIMO Receiver Tester

MIMO needs a better carrier-to-noise ratio than SISO.

MIMO offers improved spectral efficiency over SISO because, under the right circumstances, the channel capacity increases linearly with the number of transmit-receive pairs. But it doesn't come entirely for free. When comparing the performance of SISO and MIMO, the first step is to give the total transmitted signals equal power. With a direct mapped MIMO signal, this equates to requiring the carrier-(signal)-to-noise ratio, CNR, for each MIMO transmitter signal to be at least 3dB better for the same demodulation performance. This represents the point on the left hand axis in the graph of figure 5.

By introducing cross coupling, moving left to right in the graph, we can see how the CNR has to further improve as the condition number of the MIMO channel gets higher. The matrix condition number is a standard mathematical concept that indicates the potential increase in capacity for a particular MIMO channel. The poster associated with this article provides more details on how it is calculated.

In-phase (0°) coupling is a starting point for testing a MIMO receiver, as the step beyond single channel sensitivity testing. It will verify how well the channel recovery operates when the training signal has noise. For example, when a lot of coupling is applied,

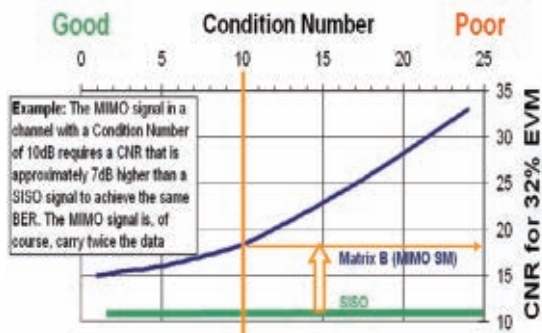


Figure 5 Results demonstrating MIMO needs a better CNR than SISO.

excess errors in the receivers' channel estimation due to insufficient processing resolution will cause receiver performance to degrade faster than expected. A further step in testing is to add a delay in the coupling, which introduces a phase variation proportionate to the OFDMA subcarrier.

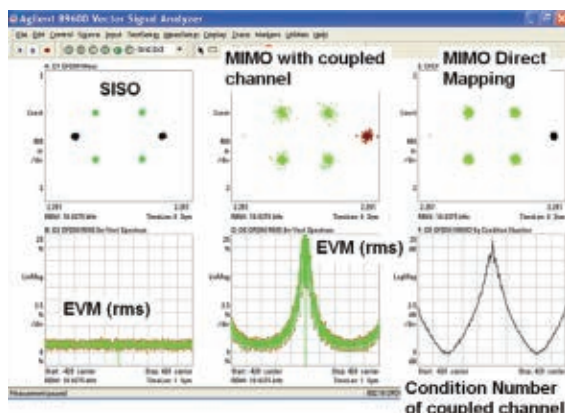
The EVM trace in the Agilent 89600 VSA display of *figure 5* shows a V-shape indicating a time delay in an OFDM signal. In this example, the signal amplitude was first adjusted to ensure there was measurement noise, resulting in a raised level of EVM (RCE). The match between the increase in EVM and the worsening condition number is clearly seen in the bottom, center and right traces.

Distortion in one component degrades all coupled codewords (streams).

In a direct-mapped configuration, where the measurement is made on individual transmitter outputs, distortion from an analog component such as an amplifier or mixer will only affect the data codeword (stream) it is carrying. If however the data signal is precoded, such as with codebook 1 or 2 in LTE, the codewords share analog components and are affected by distortion in any of them.

To create the measurements in *figure 6*, a MIMO signal was subject to the 1,1,1,-1 precoding known as codebook 1 in LTE, or spatial expansion in WLAN. The gain of one of the receiver amplifiers was set to clip the ADC.

The left-hand column shows the individual signals before the coupling was removed. One of the curious MIMO measurement effects due to correlated interference can be seen. QPSK appears as a 3*3 constellation. It is called the "constellation of constellations". Despite this, it's clear the lower signal is suffering some distortion not seen on the upper signal.



In the center column, the signals have been separated so both are QPSK, but note how both are suffering some of the distortion previously only seen on one half. Finally, the right-hand column is a transmit diversity signal fed through a system where one transmitter was distorted. The point to note is that neither signal appears distorted; indicating that only measuring fully decoded diversity signals can mask physical hardware problems.

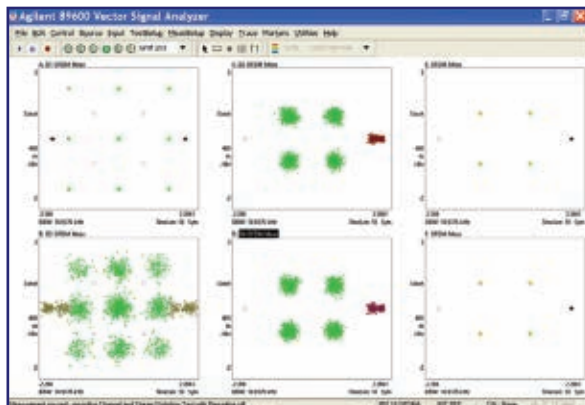


Figure 6 In the left-hand column, distortion in one channel component is seen to only affect the lower trace. The spatially multiplexed signal in the center shows both streams impaired. The right-hand trace shows how the impairment is hidden when diversity, rather than spatial multiplexing, is applied.

Summary

MIMO is an exciting addition to the transmission methods available to the radio engineer. This article has provided information relating to the key aspects of MIMO operation and measurement — showing how Agilent's design and test solutions help you ensure your receivers and transmitters are operating correctly.

Useful Resources from Agilent

To order your free copy of Agilent's new MIMO Poster "Ten Things You Should Know about MIMO" please visit www.agilent.com/find/mimo-mwj.

To view archives of Agilent's MIMO webcasts, please visit www.agilent.com/find/webcasts.

For more information on Agilent's suite of MIMO design and test solutions, please visit www.agilent.com/find/mimo.

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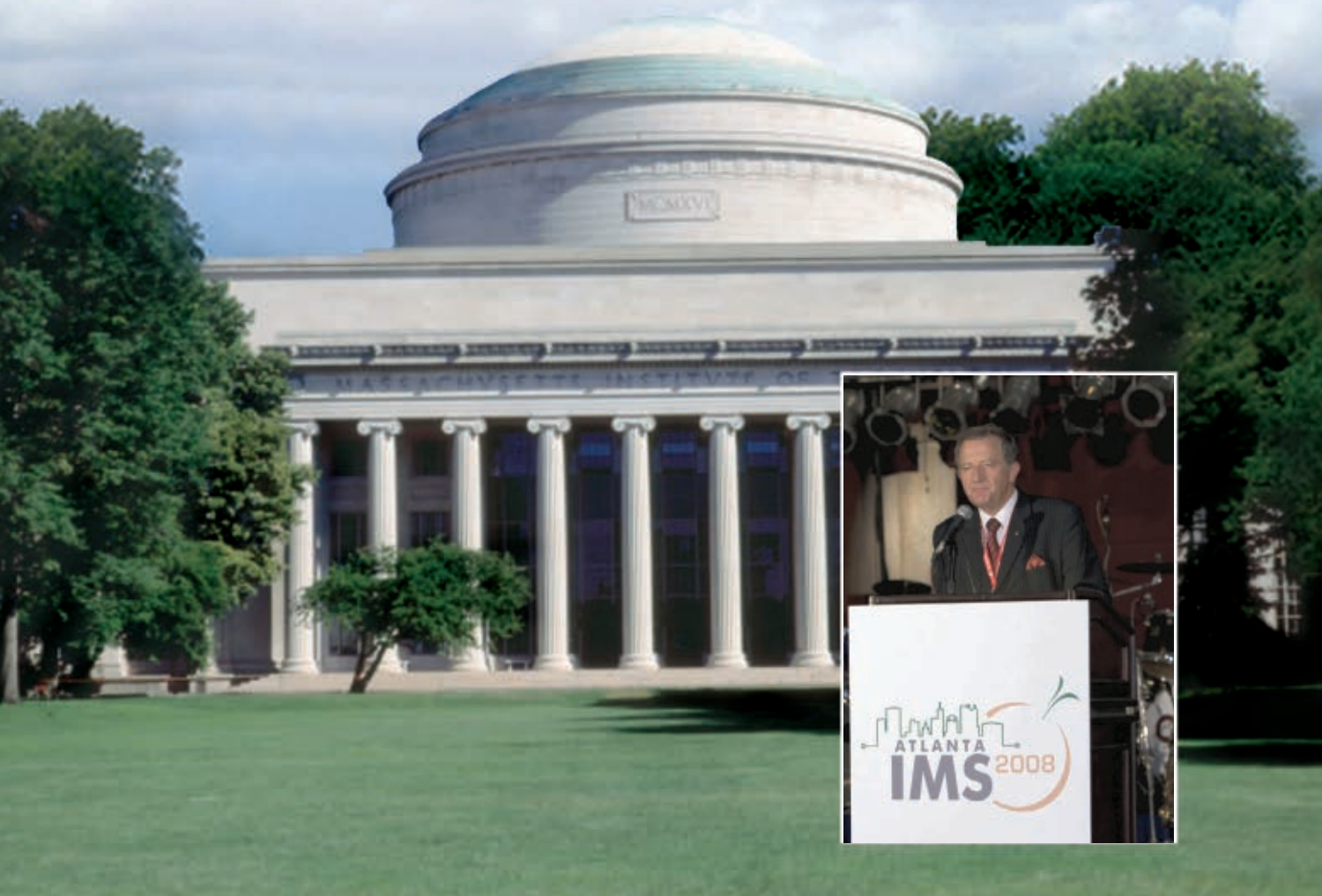


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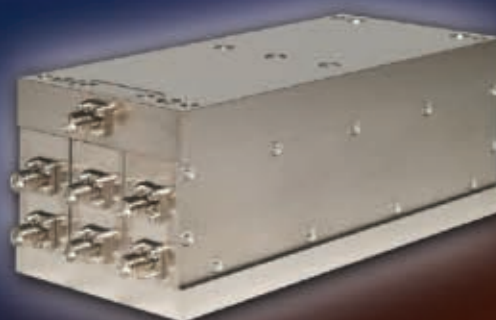
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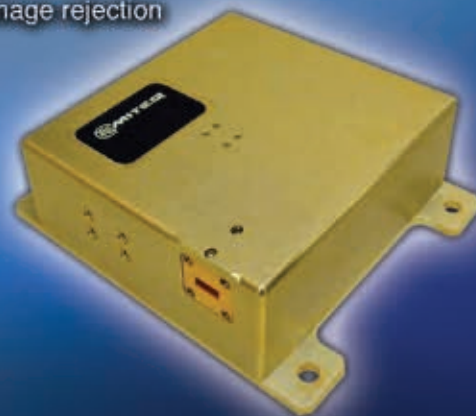
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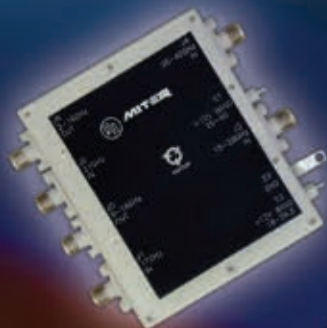
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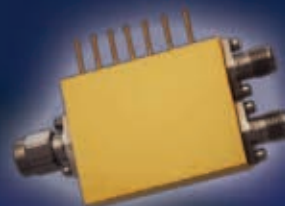
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INDUSTRY NEWS

■ **Terabeam/HXI**, also known as the Harmonix Division of **Terabeam Corp.**, was sold by its parent company, **Proxim Wireless**, to **Renaissance Electronics Corp.** (REC), Harvard, MA. Going forward, the new company name will be **HXI LLC** and HXI will be a wholly-owned subsidiary of REC. Proxim will retain the use of the Terabeam name and it will no longer be used by HXI. All management, engineering, technical, administrative and direct sales personnel have remained with HXI through the acquisition. HXI also retained all relevant intellectual property, patents and component/subsystems designs that they had previous to the acquisition. HXI will remain in the same facility and will have all the same contact information, with the exception of e-mail addresses and web site address. The company can be reached at HXI LLC, a wholly-owned subsidiary of Renaissance Electronics Corp., Ward Hill Business Park, 22 Parkridge Road, Haverhill, MA 01835; ph: (978) 521-7300; fax: (978) 521-7301 or visit: www.hxi.com.

■ **Ceralta Technologies Inc.** announced the launch of a combined direct Sales Force to support the strategic direction and valued customer base of Ceralta and its subsidiaries **TRU Corp.** and **Sage Laboratories Inc.** TRU and Sage are radio frequency and microwave solution providers that garner significant brand recognition in the marketplace due to the individual technological innovations and growing value to their customers since each was founded in the early 1950s. Ceralta's combined Sales Force will be jointly directed by Michael Wisner and Ed Kersten.

■ **Harris Corp.**, an international communications and information technology company, announced that it will integrate technology from **Freescall Semiconductor**, a global-leader in the design and manufacture of embedded semiconductors, into its new TV transmitters for terrestrial broadcasters. Using Freescall's laterally diffused MOS (LDMOS) UHF technology will enable Harris to produce its most compact and power-efficient UHF transmitters.

■ **Acceleware® Corp.**, a developer of high performance computing applications, and **Computer Simulation Technology (CST)**, a supplier of electromagnetic (EM) simulation software, announced a new Compute Unified Device Architecture (CUDA)-based Acceleware solution for accelerating EM simulations with CST MICROWAVE STUDIO® (CST MWS). Trial tests of this new acceleration product have delivered performance gains of up to 40 percent compared to the current product.

■ **Peregrine Semiconductor Corp.**, a supplier of high performance RF CMOS and mixed-signal communications ICs, and **Rubicon Technology**, a manufacturer of sapphire substrates and other advanced technology materials, announced that Rubicon has begun initial production of 8" sapphire wafers for supply to Peregrine for its UltraCMOS™ Silicon-on-Sapphire (SOS) semiconductor processing.

■ **TriQuint Semiconductor**, an RF front-end product manufacturer and foundry services provider, was recognized by **Northrop Grumman Corp.** Electronic Systems (NGES) at its 2008 Supplier Conference with an award for bulk acoustic wave (BAW) innovation. At the same event, TriQuint also received a Strategic Supplier Award for its dedication to the success of NGES programs. TriQuint was one of 32 companies recognized by Northrop Grumman at the event and the only company to win two awards.

■ **Astrolab** has received its AS9100 B certification as a manufacturer of RF and microwave applications for the aerospace industry. AS9100 B is a Quality Management System that specifies aerospace industry quality and manufacturing standards. In addition to receiving this new certification, the company was re-certified to the ISO 9001:2000 standard maintained since 1994.

CONTRACTS

■ **Skyworks Solutions Inc.**, an innovator of high performance analog and mixed-signal semiconductors enabling mobile connectivity, announced that it has signed a five-year, multi-million dollar contract with **Lockheed Martin** to supply high-precision technical ceramic toroids and inserts for the Aegis Weapon System. This contract win reflects the company's increasing diversification into adjacent markets within its Linear Products business.

■ **Nitronex**, a developer and manufacturer of high performance RF power transistors for wireless infrastructure, broadband and military markets, has received Phase II Small Business Technology Transfer (STTR) funding to further develop its GaN technology for military and aerospace applications. The two-year Phase II STTR program began in the first quarter of this year. The primary program objective is to deliver high power X-band GaN monolithic microwave integrated circuits (MMIC) that address Ballistic Missile Defense radar needs of the Missile Defense Agency (MDA).

■ **MI Technologies** has completed installation of a very large planar near-field antenna measurement system at the Naval Surface Warfare Center (NSWC Crane), located in Crane, IN. NSWC Crane provides comprehensive support for complex military systems spanning development, deployment and sustainment in three mission areas: Electronic Warfare/Information Operations, Special Missions and Strategic Missions.

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TM8-GT	8:1	5 - 1000	
TM2-GT	2:1	5 - 1500	
TM1-6	1:1	5 - 3000	
TM1-8	1:1	800 - 4000	
TM4-1	1:4	10 - 1000	
TM4-4	1:4	10 - 2500	
TM1-2	1:1	20 - 1200	



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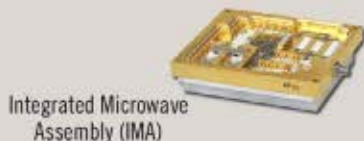


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PERSONNEL

■ The publishing and defense industries lost a respected veteran recently with the death of **Hal Gershanoff**. Hal joined Horizon House in 1978 and served as publisher of the *Journal of Electronic Defense* until his retirement in 2002, after which he continued to work with the Association of Old Crows (AOC). He travelled extensively for business and pleasure, establishing personal relationships around the globe. He leaves his wife of 35 years, Mary Dana, and a strong legacy in the industry.



▲ Harry Rutstein

■ **Harry Rutstein** has retired from the presidency of Dorado International and left the telecommunication industry for his new calling as an explorer and writer. In 1948 he started as a research engineer at Johns Hopkins University and over the next 60 years established and managed many marketing and manufacturing enterprises. Now as a writer, Rutstein announced the September publication release of *The Marco Polo Odyssey: In the Footsteps of a Merchant Who Changed the World*. The book is a personal narrative of his 13,000 mile overland journey to become the first person to follow the voyage of Marco Polo from Venice to Beijing. Rutstein can be reached via e-mail at hrutstein2@aol.com.



▲ Joe Bottenfield

■ Crane Aerospace & Electronics, a segment of Crane Co., has announced the appointment of **Joe Bottenfield** as the vice president of microwave systems solutions, which includes both the Beverly, MA and Chandler, AZ sites. Crane's Microwave Systems provide RF and microwave solutions for the defense, space and communications industries for use in electronic countermeasures, missiles, radar, intelligence and guidance systems. Prior to Crane, Bottenfield was director of avionics, North America for Barco Inc.



▲ Greg Baker

■ Mimix Broadband Inc. announced that it has appointed **Greg Baker** as senior vice president sales and marketing. Baker will focus on managing the sales cycle, acquiring new customers and expanding relationships with existing customers, and launching new products to the marketplace. Most recently with Sirenza Microdevices as vice president international sales, Baker brings more than 20 years experience in RF and microwave component design, marketing and sales to Mimix.

■ Renaissance Electronics Corp. announced the appointment of **Charles Nashef** in charge of the company's In-



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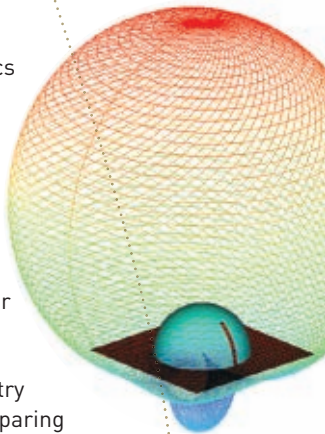
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■ **KOR Electronics** announced that **Bruce Quinn** has joined the company as director of sales. In his role as sales



▲ Bruce Quinn

director, Quinn oversees KOR Electronics' sales activities with major prime contractors and Asian customers. Prior to joining KOR Electronics, Quinn was director of sales for Crane Aerospace and Electronics. He comes to KOR Electronics with over 30 years of experience in the microwave industry.

REP APPOINTMENTS

■ **MITEQ Inc.** announced the appointment of **TriTex Technical Sales Inc.** as the company's exclusive sales representative in Texas. TriTex Technical Sales Inc. will represent MITEQ's Component division of products. TriTex Technical Sales Inc. can be contacted at (972) 492-2621 or e-mail: dpgrand@worldnet.att.net or tritex@austin.rr.com.

■ **Micro-Coax** announced the appointment of **Northern Technical Sales** as sales representative in the Upstate New York territory. Northern Technical Sales has been providing solutions for demanding test and measurement applications since 1988.

■ **Planar Monolithics Industries Inc. (PMI)**, a manufacturer of RF and microwave amplifiers, filters, log amps, phase shifters and many other components, subsystems and systems, announced the appointment of **Altaix Electronica** of Madrid as its representative in Spain. To reach Altaix, visit www.altaix.com.

■ **California Eastern Laboratories (CEL)** has signed **Elexience** to represent its growing line of IEEE 802.15.4/ZigBee radio modules. Based in Verrières-le-Buisson, Elexience will be the exclusive source for these CEL products throughout France.

■ **Presidio Components Inc.** announced the appointment of **Southeastern Sales RF LLC (SES RF)**, headquartered in Stuart, FL. SES RF will provide technical, sales representation for the Southeastern US utilizing extensive technical expertise to solve customer problems. Presidio Components manufactures quality ceramic capacitors serving commercial, defense and space markets, with unique capabilities in compact, high voltage and/or high frequency ceramic capacitors. Contact SES RF directly at (321) 431-1503 or visit them on the web at www.sesrf.com, or contact Presidio at (858) 578-9390.

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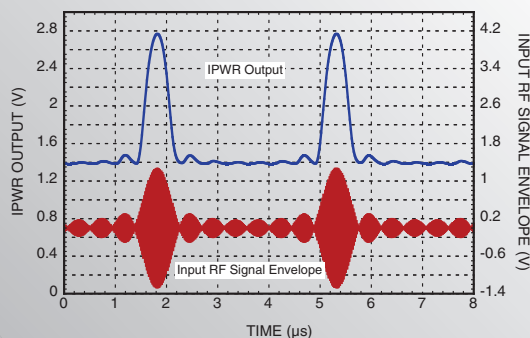


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	0.001 - 8.0	Log Detector	70 ± 3	-25	-61	+5V @ 113mA	LP4	HMC602LP4E
	0.001 - 10.0	Log Detector	70 ± 3	-25	-65	+5V @ 106mA	LP4	HMC611LP4E
NEW!	0.001 - 10.0	Log Detector	73 ± 3	-25	-65	+5V @ 103mA	Chip	HMC611
	0.01 - 4.0	Log Detector	74 ± 3	19	-68	+3.3V @ 30mA	LP4	HMC601LP4E
	0.05 - 4.0	Log Detector	70 ± 3	19	-69	+3.3V @ 29mA	LP4	HMC600LP4E
NEW!	0.1 - 3.9	RMS / PAR Power Detector	71 ± 1	37	-58	+5V @ 75mA	LP4	HMC614LP4E
	DC - 3.9	True RMS Detector	69 ± 1	37	-60	+5V @ 65mA	LP4	HMC610LP4E
NEW!	0.1 - 20	SDLVA	62	14	-57	+3.3V @ 83mA	LC4B	HMC613LC4B
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TRANSCEIVER DUPLEXER DESIGN CONSIDERATIONS

The transceiver duplexer is a key element in avionics systems, radars, antenna arrays and wireless communication systems. The duplexer provides protection of the receiver and transmitter from unwanted parasitic signals. This article discusses several duplexer schematics, their development flow and a trade-off design.

DUPLEXER SCHEMATICS

An RF transceiver duplexer connecting a single antenna to the transceiver is often the key component in phase arrays, radar, communications and navigation systems. A duplexer directs the transmitter energy to a sin-

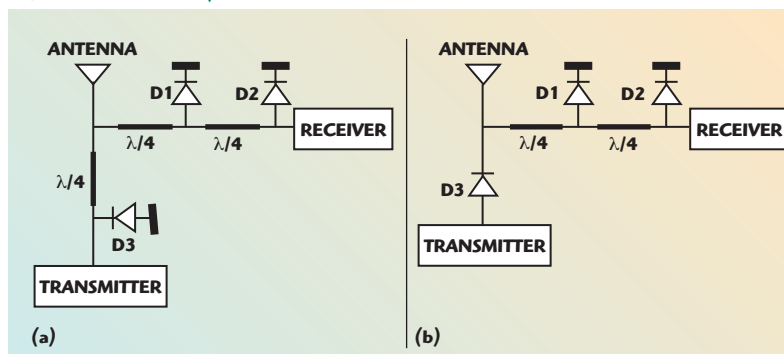
gle antenna during the transmit mode and the energy received by the antenna to the receiver during the receive mode.

The RF duplexers can be classified according to the timing of the transmit and receive operations: Full duplexer when the transmitter and receiver are operating simultaneously and half duplexer when the transmitter and receiver are operating at different times. In pulse systems, the transmit and receive time are separated. In CW systems (for instance, Doppler radars, CW altimeters, etc.), the transmit and receive modes are implemented at the same time. The duplexer is not a frequency-selective device like a diplexer and must be designed for operation in the frequency band used by the receiver and transmitter.

The duplexers should meet the following objectives:

- reduce the number of antennas (a single antenna for transmitting and receiving)
- reduce the number of cables connecting the transceiver with the single antenna
- reduce the potential transmitter pulling,

Fig. 1 TX/RCV switch/limiter duplexer directs the transmitter energy to a single antenna during the transmit mode and the energy received by the antenna to the receiver during the receive mode.



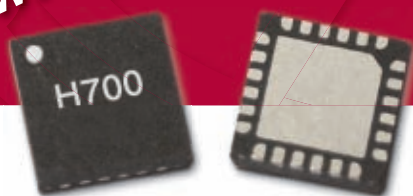
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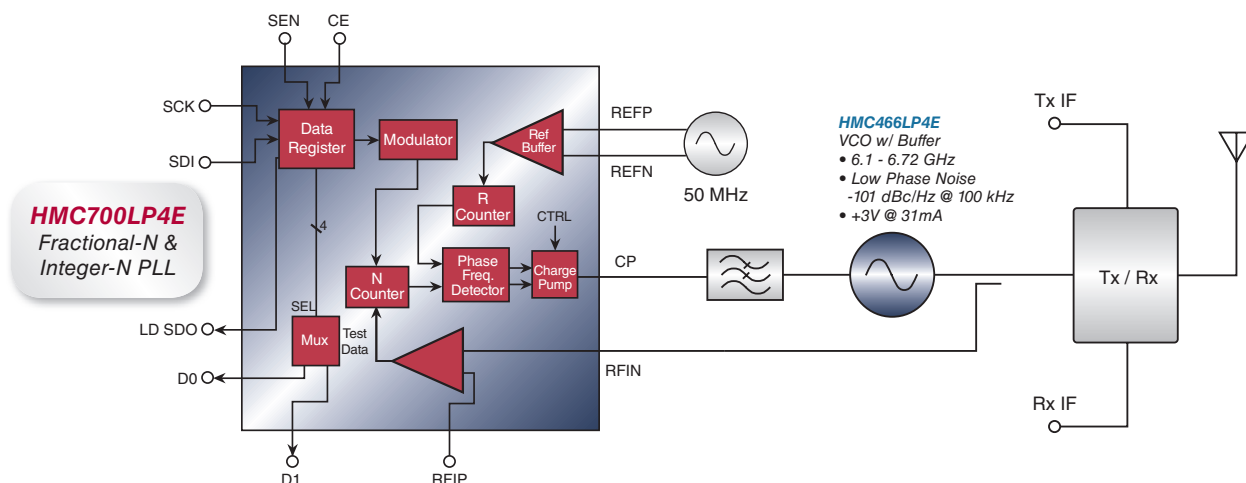


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NEW! 0.1 - 8.0	Fractional-N & Integer-N	100	200	-221 / -226	3	+5V @ 95mA	LP4	HMC700LP4E
NEW! 0.08 - 7.0	Integer-N	1300*	1300	- / -233	10	+5V @ 310mA	LP5	HMC698LP5E
NEW! 0.08 - 7.0	Integer-N	1300*	1300	- / -233	10	+5V @ 310mA	LP5	HMC699LP5E

* Maximum frequencies may be limited by available counter division ratio.

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intermodulation and noise due to antenna mismatch

- protect the receiver from unwanted (parasitic) synchronous and non-synchronous signals
- reduce cost, maintenance and mechanical complexity

The transceiver duplexer has to provide the following electrical performance:

- low transmission loss to maximize the radiated power
- minimum receive loss for low receiver noise figure and maximum receiver sensitivity
- sufficient isolation between transmitter and receiver
- proper impedance match between transmitter, antenna and receiver
- suppression of the unwanted parasitic signals in the receiver and transmitter passes
- high transmitter peak and average power

There are three main types of duplexer in common use. The first duplexer consists of an SPDT transmit/receive (TX/RCV) switch/limiter. The second type includes a ferrite circulator, while the third includes a ferrite circulator and a transceiver protector.

TX/RCV SWITCH/LIMITER DUPLEXER

Figure 1 illustrates a duplexer that includes a TX/RCV switch/limiter. Practically any PIN diode can be used in a limiter. The main difference between switch and limiter

designs is the reflection transients. Several PIN diode switch architecture options should be considered. The most important circuit configurations include: series, shunt or series-shunt PIN diodes. One of the limiters shown includes one shunt switch PIN diode D3 in the transmit pass and two shunt limiter diodes D1 and D2 in the receive pass. The other includes one series switch PIN diode D3 in the transmit pass and two shunt limiter diodes D1 and D2 in the receive path. The shunt diode switches are commonly used for systems with high isolation and are capable of handling higher power because the heat dissipation in a shunt diode (which has one grounded end) is much better than for a diode in a series-type switch due to good heat sinking. Series diode switches are commonly used in broadband circuits. The series-shunt configuration provides greater isolation than the previous version, but requires a bias current from both positive and negative sources that would significantly increase the DC power dissipation.

During the transmit mode, the biased limiter diodes provide active suppression of the synchronous transmitter leakage into the receiver. Also, during the receive mode, the limiter diodes of both schematics provide passive limitation of the unwanted and potentially damaging high-power non-synchronous signals received by the antenna from nearby systems.

The TX/RCV switch/limiter duplexer is characterized by:

- low insertion loss in order to minimize transmitter power delivered to the antenna and receiver input noise figure
- high TX-RCV isolation
- high switching speed
- low harmonic and intermodulation products
- low cost
- small physical dimensions
- good temperature stability

The TX-RCV isolation is achieved by a switch that disconnects either the transmitter or the receiver. The TX/RCV switch/limiter duplexer may not be electrically symmetrical. For example, 20 dB of isolation in the transmit arm is sufficient to prevent any variation in the output impedance of the transmitter from affecting the performance of the receiver, while more than 40 dB of isolation in the receiver arm is necessary to protect the receiver from the strong transmit signal.

A single-stage switch/limiter can typically produce approximately 20 dB of isolation, depending on the PIN diode characteristics. For a greater than 40 dB transmit-receive isolation, multi-stage limiters, such as the two-stage switch/limiter, can be used in the receive pass. The isolation of one shunt PIN diode is given by

$$a_{\text{iso}} \approx 10 \log \frac{Y^2}{4} \quad (1)$$

where $Y = 1/R_F$ is the shunt diode normalized susceptance and R_F is the diode series resistance.

For the ON diode mode, the relationship between the isolation of the two-diode shunt-iterated switch and diode resistance R_F or susceptance Y can be found¹

$$a_{\text{iso}} = 10 \log \frac{Y^2}{4} + 10 \log \frac{Y^2}{4} + 10 \log 4 \quad (2)$$

Comparing Equations 1 and 2, it can be seen that the isolation of the two shunt-iterated diodes separated by a spacing of $l = \lambda_0/4$ is double that of a single device, plus 6 dB (10 log 4) extra. The isolation of an n-diode shunt-iterated SPST switch is

TABLE I

PERFORMANCE OF HIGH POWER SM PIN DIODES

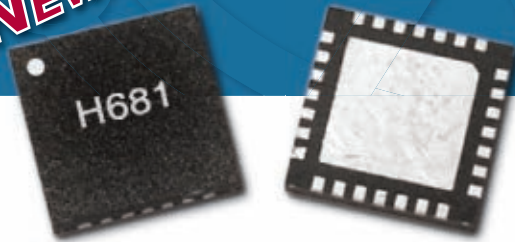
Performance	M/A-COM 4P505-1072T	MICROSEMI G C42405-M1	Test Conditions
Breakdown voltage (min) (V)	500	500	$I_R = 10 \mu\text{A}$
Series resistance R (max) (Ω)	0.45	0.8	$I_F = 100\text{mA}$, $F = 100 \text{ MHz}$
Total capacitance C_j (max) (pF)	0.65	0.55	$F = 1 \text{ MHz}$, $V_R = 100 \text{ V}$ $V_R = 50 \text{ V}$, $F = 1 \text{ MHz}$
Minority carrier life time (at 50% recovery) (max) (μS)	1.1	1.5	$I_F = 10\text{mA}$, $I_r = 6\text{mA}$
Minority carrier life time (at 90% recovery) (max) (μS)	2.2	3.0	$I_F = 10\text{mA}$, $I_r = 6\text{mA}$

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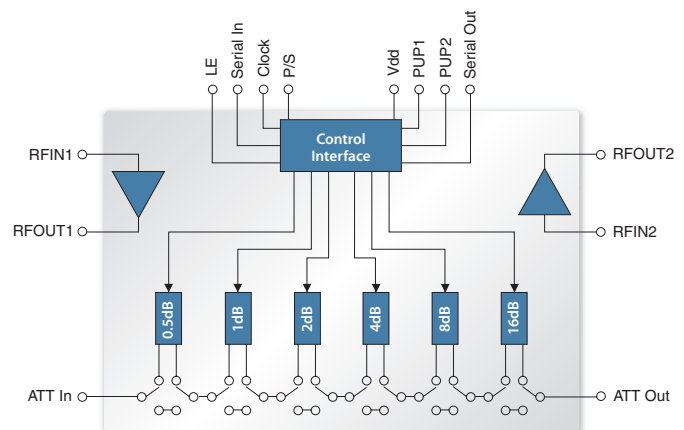
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	Frequency (GHz)	Function	Gain Control Range (dB)	NF * (dB)	OIP3 (dBm)	P1dB (dBm)	Bias Supply	Package	Part Number
	0.4 - 3.0	Analog VGA	-25 to +20	5	40	23	+5V @ 265mA	LP5	HMC640LP5E
NEW!	6 - 17	Analog VGA	+1 to +23	5	30	22	+5V @ 170mA	Chip	HMC694
	0.05 - 0.8	5-Bit Digital	-8 to +15	5	35	18	+5V @ 65mA	LP4	HMC628LP4E
	DC - 1	6-Bit Digital, Serial & Parallel Control	-11.5 to +20	4.3	36	20	+5V @ 90mA	LP5	HMC627LP5E
	DC - 1	6-Bit Digital, Parallel Control	+8.5 to +40	4	36	20	+5V @ 176mA	LP5	HMC626LP5E
NEW!	DC - 1	6-Bit Digital, Serial Control	+13.5 to +45	2.7	36	20	+5V @ 176mA	LP5	HMC681LP5E
	DC - 6	6-Bit Digital, Serial & Parallel Control	-13.5 to +18	6	33	19	+5V @ 88mA	LP5	HMC625LP5E

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$$a_{\text{iso}} = n \times 10 \log \frac{Y^2}{4} + (n-1) \times 6 \text{ (dB)} \quad (3)$$

The TX/RCV switch duplexer has the following disadvantages:

- no protection to the transmitter from the transmitter power reflected from the antenna mismatch and from other elements

in the TX/RCV common channel


- power-handling capability limit
- switching speed limit
- necessity of control signals
- possible harmonics and inter-modulation product

The three quarter-wavelength sections narrow the bandwidth to approximately 10 percent. The operating bandwidth can also be limited by the diode bias network, which is a fil-

ter network that isolates the DC bias current from the RF network. To increase the bandwidth and minimize the transmit insertion loss, the distance from the series diode D3 to the common junction should be an absolute minimum. There are different switch modifications with greater bandwidth. The Hewlett Packard network,² which includes additional transformers with other than 50 Ω

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Model	Bandwidth	Low Frequency 3dB	Max DC Voltage	Max DC Current
5530A	12.5 GHz	20 KHz	200 V	10 mA
5531	10 GHz	750 KHz	1.5 KV	20 mA
5541A	>26 GHz	80 kHz	50 V	100 mA
5542	50 GHz	10 kHz	16 V	100 mA
5542K	40 GHz	12 KHz	16 V	100 mA
5542LL	>40 GHz	12 kHz	16 V	100 mA
5545	20 GHz	65 kHz	50 V	500 mA
5546	7 GHz	3.5 KHz	50 V	500 mA
5547	15 GHz	5 kHz	50 V	500 mA
5550B	18 GHz	100 kHz*	50 V	500 mA*
5575A	12 GHz	10 kHz*	50 V	500 mA*
5580	15 GHz	10 kHz	50 V	2 Amp
5585	18 GHz	2 GHz	100 V	6 Amps
5586	5 GHz	1 GHz	100 V	8 Amps
5587	2 GHz	200 MHz	100 V	6 Amps
5589	2.8 GHz	300 MHz	100 V	7 Amps
SM100	13 GHz	14 kHz	16 V	500 mA
SM101	15 GHz	7 kHz*	16 V	500 mA

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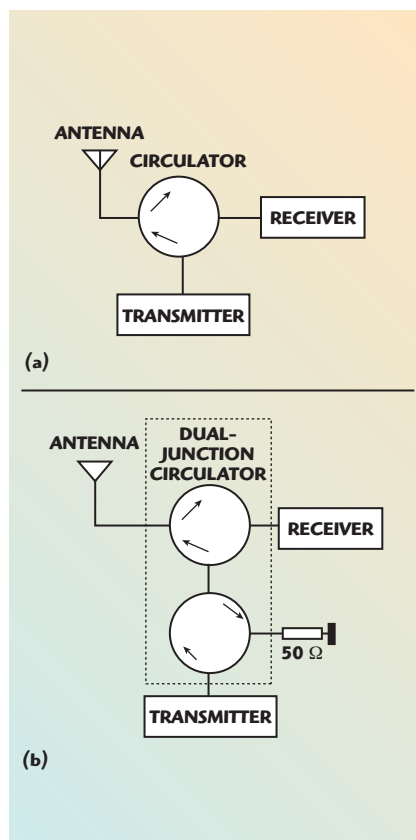
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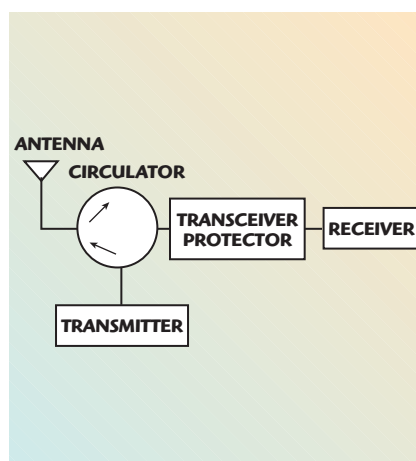
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▲ Fig. 2 TX/RCV duplexers using circulators.



▲ Fig. 3 TX/RCV duplexer using a circulator and a transceiver protector.

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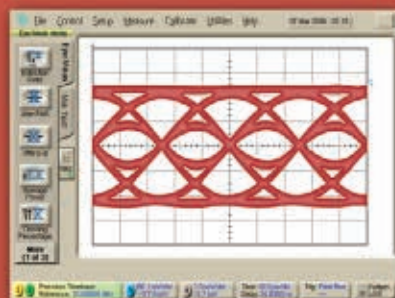
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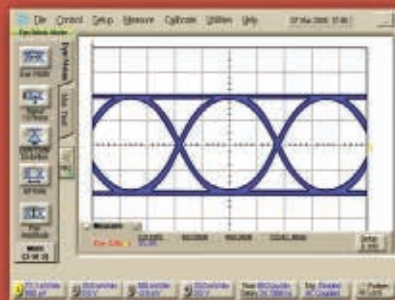
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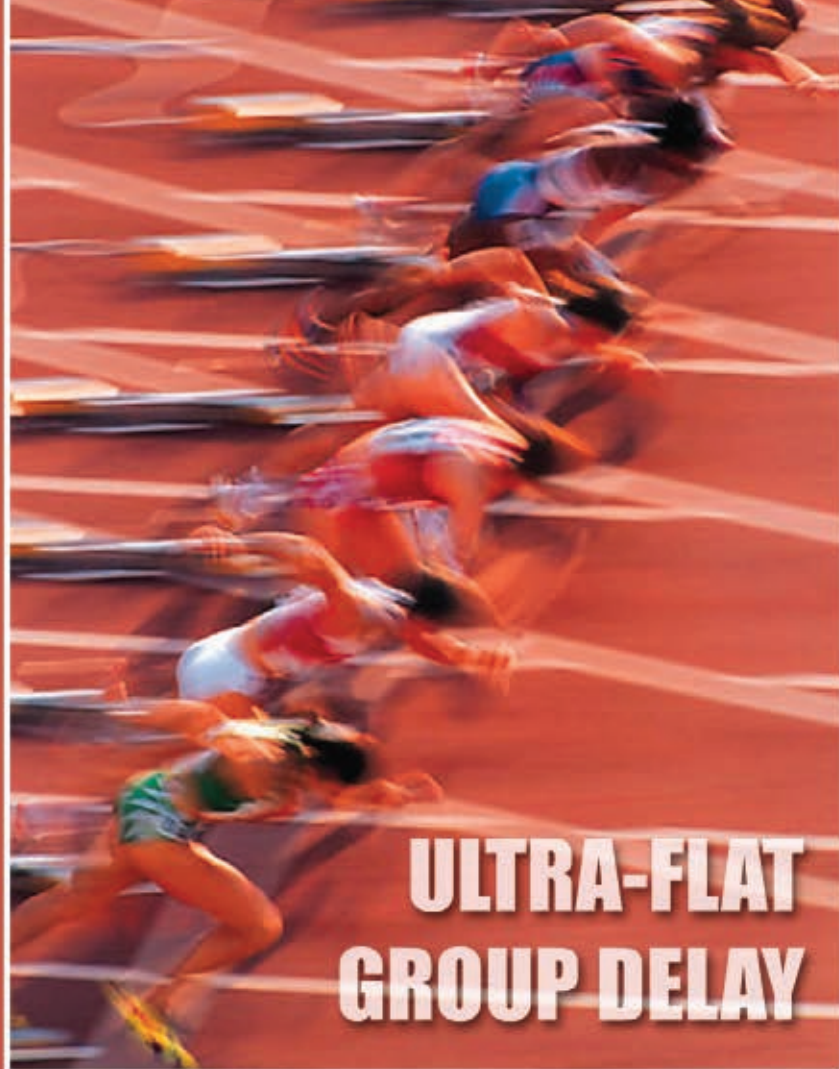
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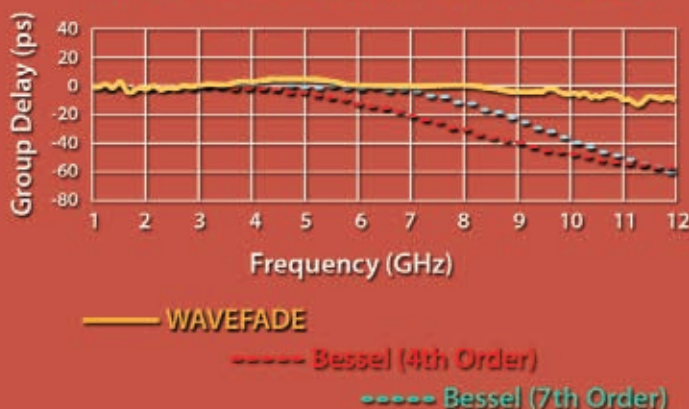


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impedances, provides a bandwidth greater than 30 percent. Also, to improve bandwidth, a series-shunt diode network can be used.

The conventional narrow-band shunt diode switch topology with quarter-wave diode spacing is too large at low frequencies. A defected ground structure (DGS)³ can provide reduction of size and harmonic signal. A DGS switch shows results very

comparable to a conventional switch, in spite of being half the size.

For a good switch performance, the PIN diodes should have a low resistance at low forward current and low capacitance at zero bias. **Table 1** illustrates the performance of two high-power surface-mount PIN diodes.

The TX/RCV switch must rapidly disconnect the transmitter and con-

nect the receiver to the antenna. The switching speed limit depends on the PIN diode carrier life time. PIN diode switches can generate harmonics and intermodulation products since PIN diodes are fundamentally nonlinear devices. All distortions are strongly influenced by the lifetime of a PIN diode, as well as the transmitter RF power which is applied to the diode. The contradictory requirements for the switch diode will be discussed later.

CIRCULATOR DUPLEXER

The duplexers in **Figures 2** and **3** include a circulator whose principal role is to protect the expensive, high power, TX RF power amplifier from variation in loading conditions.

The circulator network provides:

- greater maximum power
- no need for electrical switching
- additional attenuation (approximately 6 to 8 dB) to the different harmonics⁴

In the full duplexer, transmission and reception can occur simultaneously. The main problem is that the isolation of a circulator is poor. Therefore, an antenna mismatch results in poor transmitter-receiver isolation and transmitter pulling due to the signal reflected from the mismatched receiver.

To improve circulator isolation, different options can be used. Dual-junction circulators are used in high-power systems requiring high receive-transmit isolation (up to 50 dB) and transmitter stability. With the isolator installed in the network, any reflected power will flow into the 50 Ω load of the isolator and is dissipated into heat. A three-dimensional dual-junction circulator¹ provides a high integration level in the horizontal plane and low cost as compared with traditional multi-junction circulators.

Another circulator duplexer option is a network with a three-port circulator and a transceiver protector that provides:

- greater isolation
- protection of RCV from synchronous and non-synchronous signals
- protection of TX from reflection signal from antenna and other elements in the TX/RCV common channel



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VMMK-2503*	1.0 - 12	5	60	3	3.7	14	+17	+28	50 ohm RFIC

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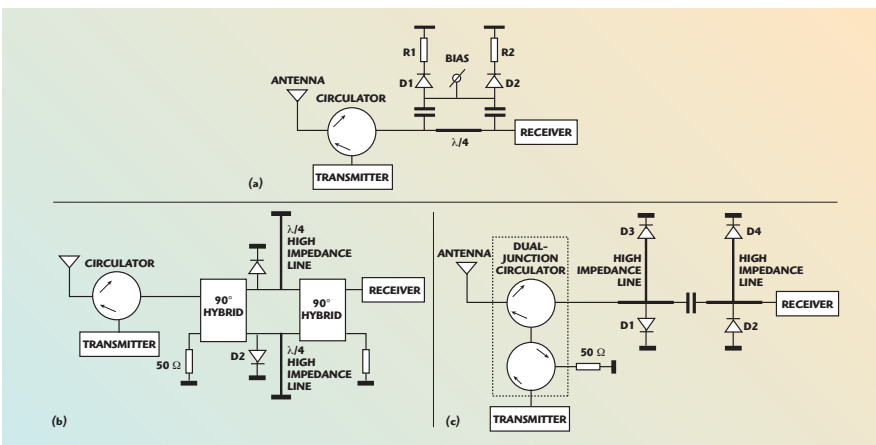


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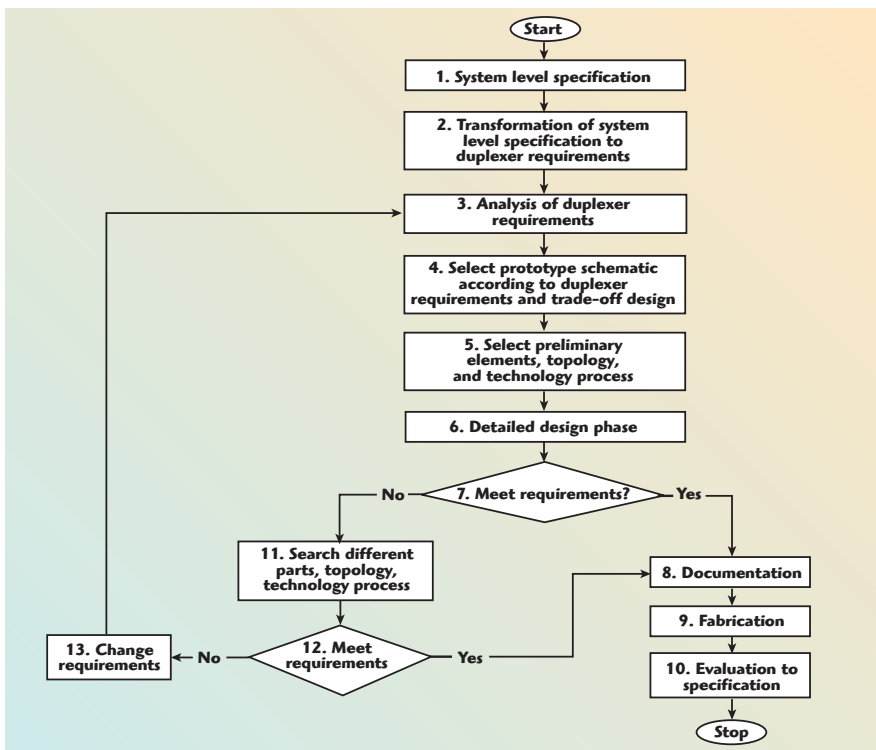
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TABLE II
DROP-IN 3 PORT CIRCULATORS

Model Number	Company	Ins. Loss (dB) max	ISO (dB) min	VSWR max	Operating Temp. (°C)	Size (in)
C096012/DA	Trak	0.5	19	1.3	-25 to +85	1.5 x 1.5 x .50
		0.5	18	1.3	-40 to +85	1.5 x 1.5 x .50
3G2NF	REC	0.4	18	1.3	-55 to +24	1.25 x 1.25 x .35
		0.3	20	1.25	+25 to +85	
JID0960T1215G1	JQL	0.4	20	1.25	-30 to +70	1.00 x 1.122 x .472
		0.6	18	1.3	-55 to +85	
DFN2540-T0001	MICA Microw.	0.6	17	1.35	-55 to +85	1.00 x 1.00 x .50
SDC-0913	SMT	0.4	20	1.25	-55 to +85	1.00 x 1.00 x .30
CD-1090-S	UTE Microw.	0.6	20	1.3	-30 to +85	1.00 x 1.00 x .25



▲ Fig. 4 Three types of transceiver protector configurations.



▲ Fig. 5 Duplexer development flow.

- greater maximum RF power

It is possible to maintain high circulator isolation by using an additional compensation network^{1,5} where the parasitic leakage signal is compensated for by an input signal sample. Emerging new principles and technologies offer possibilities of fabricating low cost nonreciprocal devices without using ferrites. Several designs utilizing an active circulator have been described in the literature.^{1,6-8} However, these devices possess power handling limitations.

Table 2 illustrates the performance of different L-band high-power ferrite drop-in circulators for the frequency range 960 to 1215 MHz, which can be used as duplexers in several pulsed avionics systems: DME, TCAS, Transponder and UAT.

These circulators are characterized by:

- insertion loss less than 0.5 dB
- isolation greater than 18 dB
- VSWR<1.3
- peak power handling of 600 W min

COMPARISON OF DIFFERENT DUPLEXERS

Table 3 illustrates the performance of the three kinds of duplexer. According to the table, the networks with circulators have the following disadvantages as compared to the PIN diode switch duplexer:

- higher cost
- greater dimensions
- poor temperature performance
- greater insertion loss
- required magnetic shielding

The duplexers with TX/RCV switch/limiter have the following disadvantages:

- no protection of transmitter from reflected synchronous signals
- lower peak power
- required switching control network

TRANSCIVER PROTECTOR

The transceiver protector provides:

- protection of the receiver from large input signals while allowing the receiver to function normally when these large signals are not present
- protection of the transmitter from signals reflected from the

receiver due to receiver and antenna mismatch

In the duplexer with a circulator, the transmitter power may leak into the receiving system due to non-ideal circulator isolation, antenna port reflection paths, as well as to mutual coupling from adjacent antenna array elements. This can cause such problems as saturation, gain compression of the receiving system and increased FM-AM noise. Any losses between antenna and low noise amplifier (LNA) directly degrade the receiver sensitivity. Also, sometimes unwanted and potentially damaging high-power signals from nearby systems (non-synchronous signals) received by the antenna pass to the receiver. The transceiver protector is primarily used to protect the power-sensitive receiver components and devices (LNA, mixer) from these high-power sources. The transceiver protector can also suppress the unwanted signals reflected from the antenna and the mismatched receiver to prevent transmitter pulling and possible damage. Therefore, the transceiver protector provides protection of both the receiver and the transmitter from the unwanted signals.

There are three types of the transceiver protector configurations,¹ as shown in **Figure 4**. The active limiter works on a separate current source (a). To protect the transmitter from the signal reflected from the active limiter, a non-reflective network can be used. For this network, the terminating impedance is developed by the non-reflective (absorptive) switch including the series combination of the diode and the terminating load to ground. Parasitic signals from mismatches at the antenna and TX leakage are absorbed by the limiter with $50\ \Omega$ loads. The required $50\ \Omega$ terminating impedance is achieved by the series combination of the PIN diode and terminating resistance to ground. The non-reflective (absorptive) limiter with $50\ \Omega$ loads can protect the transmitter from the reflection signals. But in the absorptive switches, the power-handling ability is limited by the ability of the diodes and resistors to dissipate RF power. The active transceiver protector can only protect against signals that are synchronous with the transmitter pulse. Protection against non-synchronous, external

TABLE III
PERFORMANCE OF THE THREE DUPLEXERS

<i>Performance</i>	<i>Duplexer Schematic</i>		
	<i>TX/RCV SPDT Switch (Fig. 1)</i>	<i>Circulator (Fig. 2,b)</i>	<i>Circulator with Transceiver Protector (Fig. 3)</i>
TX insertion loss max (dB)	0.2	0.4	0.4
RCV insertion loss max (dB)	0.4	0.4	0.8
TX-RCV isolation min (dB)	50	20	50
RCV-TX isolation min (dB)	20	40	40
VSWR max	1.3	1.3	1.3
Protection of TX from unwanted reflected synchronous signals	No	Yes	Yes
Protection of RCV from non-synchronous RF signals	Yes	No	Yes
Transmit power peak max (W)	800	1500	1500
Electrical switching	Yes	No	Yes
Switching speed limitation	Yes	No	Yes
EMI shielding problem	No	Yes	Yes
Temperature limits @-55° to +85°C	No	Yes	Yes
Package	Surface-mount	drop-in	Surface-mount diodes & drop-in circulator
Size	small	large	medium
Cost	low	high	medium

TABLE IV
PERFORMANCE OF THE THREE TYPES OF TRANSCEIVER PROTECTORS

<i>Transceiver Protector Configuration</i>	<i>Advantages</i>	<i>Disadvantages</i>
Passive (Fig. 4, b)	No power supplies required Protection from synchronous and non-synchronous RF pulses Protection from TX pulling High reliability	Switching speed limitation Large size High cost Bandwidth limitation
Active (Fig. 4, a)	Protection from synchronous RF pulses Protection from TX pulling High switching speed	DC power supplies required No protection from non-synchronous RF pulses Less reliability due to driver circuit components Bandwidth limitation
Quasi-Active (Fig. 4, c)	No power supplies required Protection from synchronous and non-synchronous RF pulses High switching speed Protection from TX pulling	Large size Less reliability due to Schottky diodes

signals is provided by the passive limitation of diodes D1 and D2. Absorptive switches exhibit slower switching speed. In some duplexers, the broadband matching is more important than the switching speed.


A duplexer with a circulator and a balanced passive limiter,⁹ which provides better switching speed performance, is also shown (b). The balanced limiter makes use of the features of two 3 dB hybrids, in

combination with limiter diodes placed between two 90° hybrids, to control the power flow. The input splitter divides the input RF signal equally between two limiter diodes. The output combiner recombines the output signals from the splitter. The balanced limiter is a non-reflective network because the reflected signals are dissipated in the input hybrid 50 Ω loads, which prevents transmitter load pulling. The hybrids of the bal-

anced configuration provide a good input and output match at all power levels and a route for the reflected power to the 50 Ω load. The limiter diodes are turned on by the RF signal itself. The passive limiter can include an RF choke inductor as well as a quarter-wave shorted high impedance transmission line. This structure allows a DC signal to pass through, but not an RF signal. In most limiter circuits, DC blocking capacitors are included at the input and the output of the circuit. These series capacitors have low series reactance at the RF frequency and allow to separate the DC current along a transmission line.

A passive limiter is a self-activated switch that is activated by a high-level incident power. The speed of this process depends on the diode lifetime (see Table 1). This relatively slow process leads to a high dissipation power on the diode. The maximum signal RF power that a limiter diode can handle is limited by either the diode's breakdown voltage or its power-dissipation capability. The absorptive passive limiter usually exhibits somewhat slower switching speeds.

To eliminate the limiter diode speed problem, a quasi-active limiter (c) can be used. Also, the quasi-active limiter provides both synchronous and non-synchronous protection of the receiver. A two-stage quasi-active limiter with limiter diodes D1 and D2 and two Schottky detector diodes D3 and D4¹ is shown. The Schottky diodes D3 and D4 are cou-



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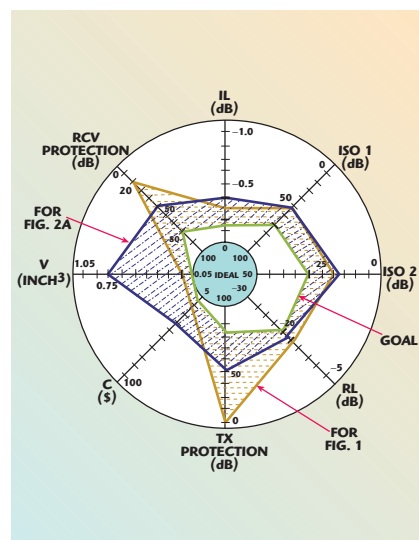
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▲ Fig. 6 Circle diagram of the duplexer parameters.

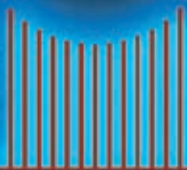
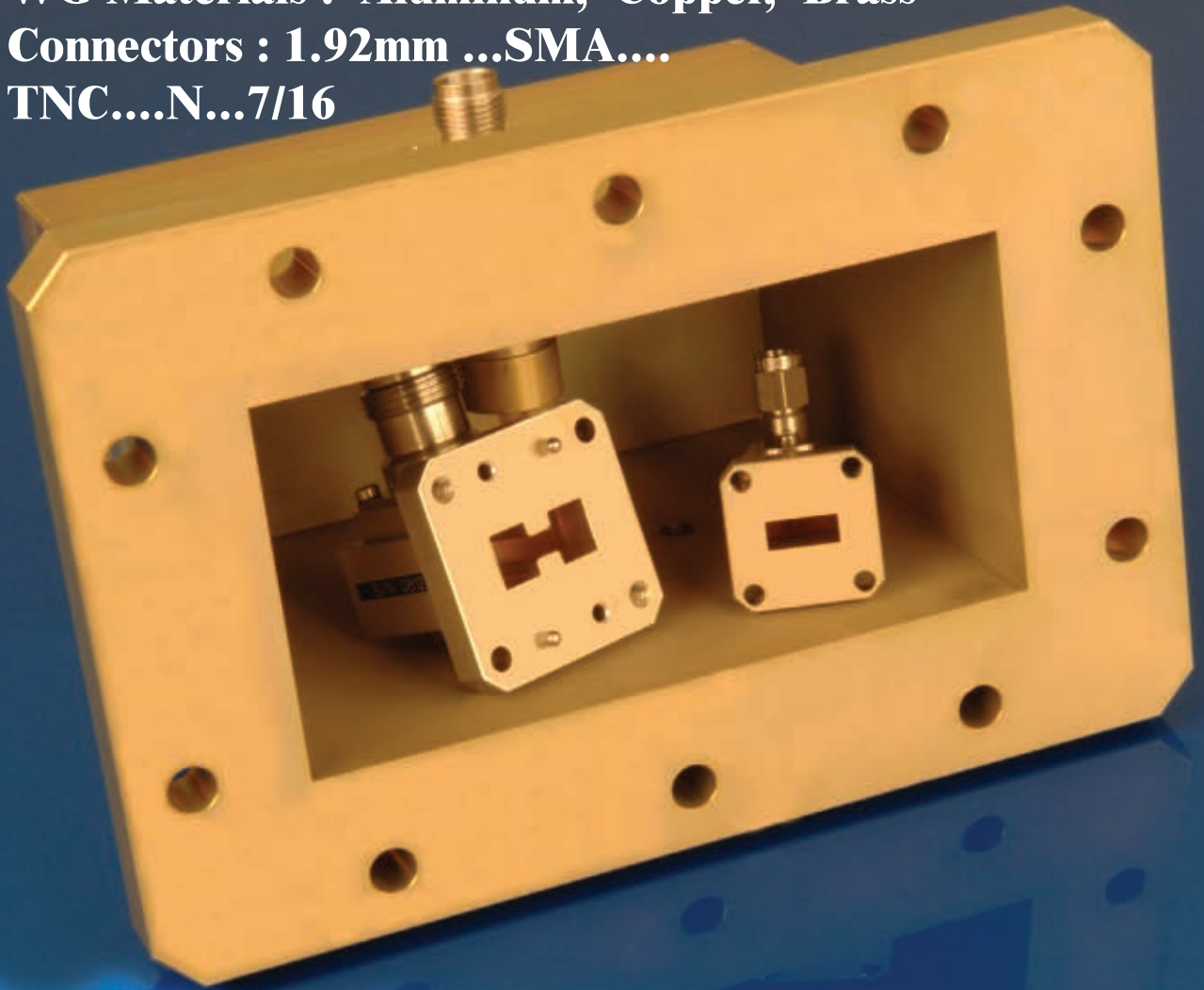
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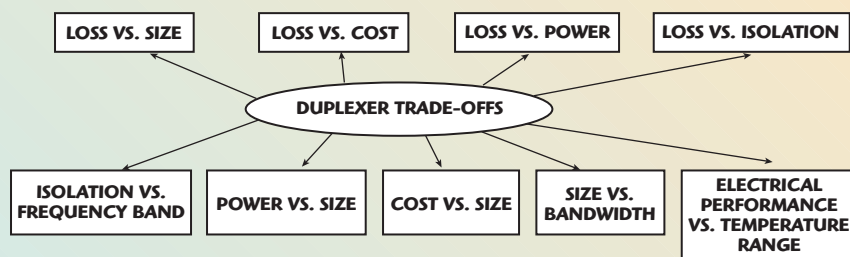
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▲ Fig. 7 Different duplexer trade-offs.

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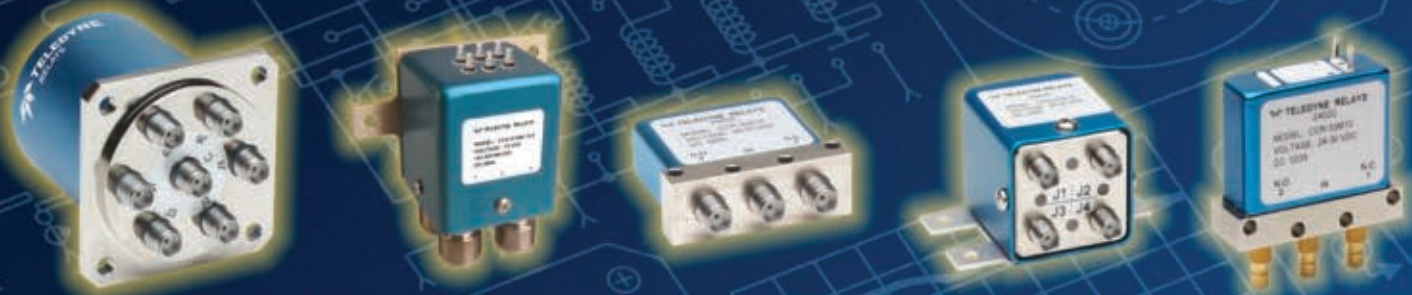
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pled (~ 20 dB) with the main $50\ \Omega$ transmission line through a high-impedance ($\sim 120\ \Omega$) transmission line or can be connected through a directional coupler. The limiter diodes D1 and D2 are turned on primarily by the external bias current from the Schottky detector diodes D3 and D4, which are sensitive to the incident signal. Diodes D3 and D4 detect the incident RF power and rapidly apply self-rectified current to the limiter diodes D1 and D2 respectively, causing a rapid increase in attenuation and protection from synchronous and non-synchronous signals. The first Schottky diode D3 starts activating the first high-power limiter diode D1 at approximately 15 dBm incident power. Diode D1 is used as a prelimiter of the high-incident RF power. The second low-power limiter diode D2 has a faster response and, therefore, provides protection during the initial stages of pulse rise time. The parasitic signals reflected from the limiter are dissipated in the dual-junction circulator $50\ \Omega$ load. This network prevents transmitter load pulling and leakage of unwanted high RF power to the receiver. **Table 4** illustrates the performance of the three transceiver protectors.

DUPLEXER DEVELOPMENT FLOW

Figure 5 illustrates the ANT/TX/RCV duplexer design flow. The system level specification is the first step in a duplexer design flow. The second step is the transformation of system level specification into the duplexer requirements. Some duplexer requirements should be similar to the system requirements; for example, frequency range, maximum power and temperature range. Other duplexer requirements are specific to the duplexer and depend on system requirements; for example, TX and RCV pass insertion loss, TX-RCV iso-

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lation and RCV-ANT isolation.

Analysis of RF duplexer requirements (third step) includes the definition of fixed and variable characteristics. Fixed duplexer characteristics are similar to the system requirements and include center frequency, bandwidth, power, etc. The variable duplexer parameters may be flexible and depend on system requirements, performance of other subsystems and devices, and physical

implementation of the duplexer network. The variable duplexer characteristics are insertion loss, isolation, matching, cost and size. A designer has to choose the weighting coefficients k_i for each duplexer parameter to provide multi-parameter optimization.

The fourth step is the selection of a prototype schematic according to duplexer requirements, analysis of the schematic and the optimum

topology trade-off design. After that, the layout can be prepared. The fifth step includes selection of elements (parts), topology and technology process. The sixth step is the detailed design phase that includes calculation and simulation over the specified temperature range and manufacturing tolerances. The final steps (8, 9 and 10) are preparation of documentation, fabrication and evaluation to specification.

Analysis of the duplexer includes multi-parameter optimization for the following major characteristics:

- TX Insertion Loss (IL)
- TX-RCV Isolation (ISO1)
- RCV-TX Isolation (ISO2)
- Matching (VSWR or Return Loss RL)
- RCV and TX protection
- Cost (C)
- Volume (V)

Figure 6 illustrates the circle diagram of these parameters with goal values (green) for the two options: 1) SPDT TX/RCV switch shown in brown and 2) circulator with transmitter-receiver protector shown in blue. To optimize the duplexer network, the area between real and goal performance should be minimized. The comparison of the two networks using the circle diagram showed that the SPDT TX/RCV switch corresponded to a smaller area and, therefore, a better performance than the circulator with transmitter-receiver protector. These preliminary results should be corrected using the weighting coefficients for each parameter. A designer has to choose the weighting coefficients k_i for each parameter from $k=1$ (most important) to $k=\max$ (least important). The circle diagram should be corrected by using different scales for each parameter according to the weighting coefficients and final decision about the optimal network should be based on a new circle diagram.

DUPLEXER TRADE-OFF DESIGN

The most contradictory duplexer parameters include (see **Figure 7**):

- loss vs. isolation, power, volume and cost
- isolation vs. frequency band
- size vs. power, cost and bandwidth
- electrical performance vs. temperature range

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The most important electrical parameter of the transceiver duplexer is insertion loss (IL). The trade-off design can satisfy contradictory parameters: insertion loss versus volume. The integration quality of these two parameters is characterized by the insertion loss – volume integration index:¹

$$i = \frac{IL}{k_1} \times \frac{V}{k_2} \left(\text{dB} \times \text{inch}^3 \right) \quad (4)$$

where IL is the total insertion loss in dB, k_1 is the weighting coefficient of the insertion loss, V is the volume in inch^3 and k_2 is the volume weighting coefficient. The optimum duplexer has the minimum integration index i_{\min} , which means the smallest physical dimensions and the minimum insertion loss. It is important to keep in mind that the integration index varies linearly with frequency.

Size (volume) of the duplexer depends on electrical requirements, transmission line type, dielectric substrate parameters, component dimensions and the structure of the duplexer. The integration strategy of a duplexer is based on the optimum schematic and design. A number of different transmission lines are generally used in RF and microwave integrated circuits. The trade-off design showed that the combination of different transmission lines offers certain advantages in both cost and insertion loss.¹

The main trends in integrated technology are smaller size and lower cost. Integrated circuits can be divided into three categories: hybrid microwave integrated circuits (HMIC), monolithic microwave integrated circuits (MMIC), and combination of hybrid and monolithic MICs. Two categories, including monolithic MICs, have high cost. The printed circuit board (PCB) technology has advantages of low cost, low loss and ease of manufacture. The disadvantage of the PCB technology is the use of plastic dielectric substrates with relatively low dielectric constant leading to greater dimensions.

The guidelines that provide the network cost reduction are listed below:

- use the cheapest technology process (PCB)
- use a low cost carrier substrate
- choose the simplest transmission line (for instance, microstrip line)
- keep the assembly as simple as possible
- avoid using expensive components
- design the TX/RCV network with minimum interconnections

For the high power circulator duplexer, requirements for very low insertion loss and high peak power are frequently in conflict. The important factor is the amount of power that the circulator can handle before nonlinearity is produced in the ferrite, which causes an increase in insertion loss. Therefore, a trade-off in the ferrite material selection is required.⁴ According to Table 2, circulators with tighter electrical performance necessarily have reduced operating temperature ranges.

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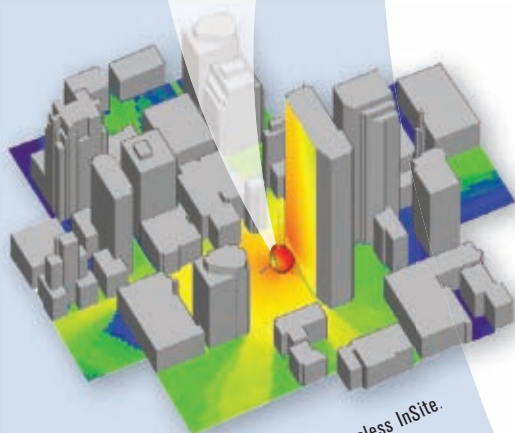
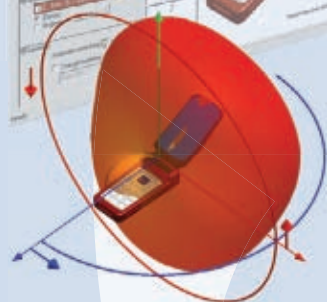
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For the TX/RCV switch/limiter and the TX/RCV using a circulator and transceiver protector duplexers, the PIN diodes and Schottky diodes are selected using the trade-off design with respect to the following conflicting performance factors: power handling, bandwidth, loss-isolation and switching speed.¹⁰ There is a direct trade-off between isolation and insertion loss in PIN diode switches:

the higher isolation, the higher the insertion loss. A designer has to specify the minimum acceptable isolation to get the lowest insertion loss. For good switching speed performance, the PIN diodes should have low capacitance at zero bias and low resistance at low forward current. To handle the high power, the limiter diode should have a high breakdown voltage and large junction area. The large

area leads to high capacitance, causing a poorer isolation than a low power device. The higher the operating frequency of the diode, the smaller the percentage of bandwidth over which high performance can be maintained. There are contradictory conditions for the diode power handling versus frequency: the junction capacitance should be at a minimum (smaller junction area) to provide low loss at high frequency. However, reducing junction area increases thermal resistance and hence reduces power handling capability. ■

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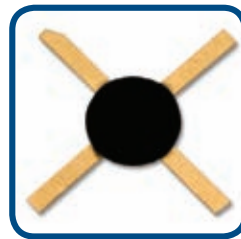
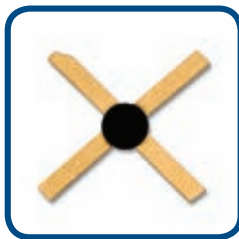
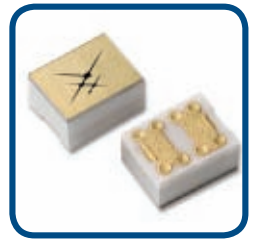
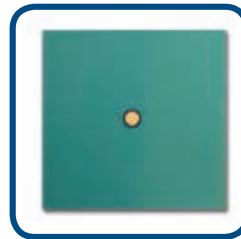
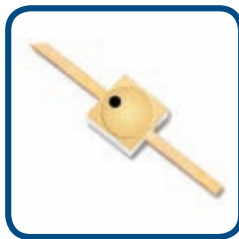
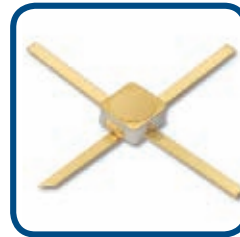
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Leo G. Maloratsky received his MSEE degree from the Moscow Aviation Institute and his PhD degree from the Moscow Institute of Communications in 1962 and 1967, respectively. In 1962, he joined the Electrotechnical Institute where he was involved in the research, development and production of RF and microwave integrated circuits and was an assistant professor. From 1992 to 1997, he was a staff engineer at Allied Signal. In 1997, he joined Rockwell Collins, where he works on RF and microwave integrated circuits for avionics systems.



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MICROWAVES IN EUROPE: HISTORICAL MILESTONES AND INDUSTRY UPDATE, PART II

Part I of this report last month focused on individual countries and their contributions and achievements related to the microwave industry. But the continent as a whole plays a key role in all sectors including industrial, biomedical, military, aerospace and emerging wireless technologies. Since there is such a broad range of sectors, in Part II we will only focus on the technological development in Europe of two sectors: Satellite communications from the launch of Sputnik to the use of satellites for mobile communication and broadcast TV; and microwave radar, which has developed to span the vastly differing demands of conflicts from WWII to the fight against terrorism to more peaceful applications such as automotive.

SATELLITE COMMUNICATIONS IN EUROPE: A HISTORICAL PERSPECTIVE

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Satellite communications is an important part of telecommunications, and the main function of satellite-based commercial systems, alongside navigation and Earth observation. A satellite placed in a geostationary orbit (GEO) fixed above the Earth has the capability to cover up to a quarter of the Earth's surface (except for the polar regions) and to realize long distance transmissions between users separated by a distance of several thousands of kilometres.

Satellite communication systems offer many different services for different groups of users, independently from the terrestrial

telecommunications infrastructure. In general, these services can be divided into two groups:

Services for stationary users

- Two-way transmission Fixed Satellite Services (FSS) and broadcast applications - Direct Broadcast Services (DBS)
- Broadcast of digital TV programmes in DVB-S and DVB-S2 standard
- International telephony connections
- Data transmission networks - i.e. Very Small Aperture Terminals (VSAT) networks
- Occasional transmissions
- Back-up for terrestrial systems

Services for mobile users - Mobile Satellite Services (MSS)

- Voice and low rate data transmission
- Broadcasting of radio programmes (XM Radio and Sirius in US)
- Future broadband interactive services - to realize communications, "anywhere and at any time"

Broadcasting of TV programmes to individual users—Direct To Home (DTH)—is a major driving force for satellite communications. Conversion to High Definition TV (HDTV) will be an additional impulse to growth as will multimedia broadband services for mobile users. Currently there are over 200 active communications satellites in GEO, with more than 100 in Low Earth Orbit (LEO).

RICHARD MUMFORD

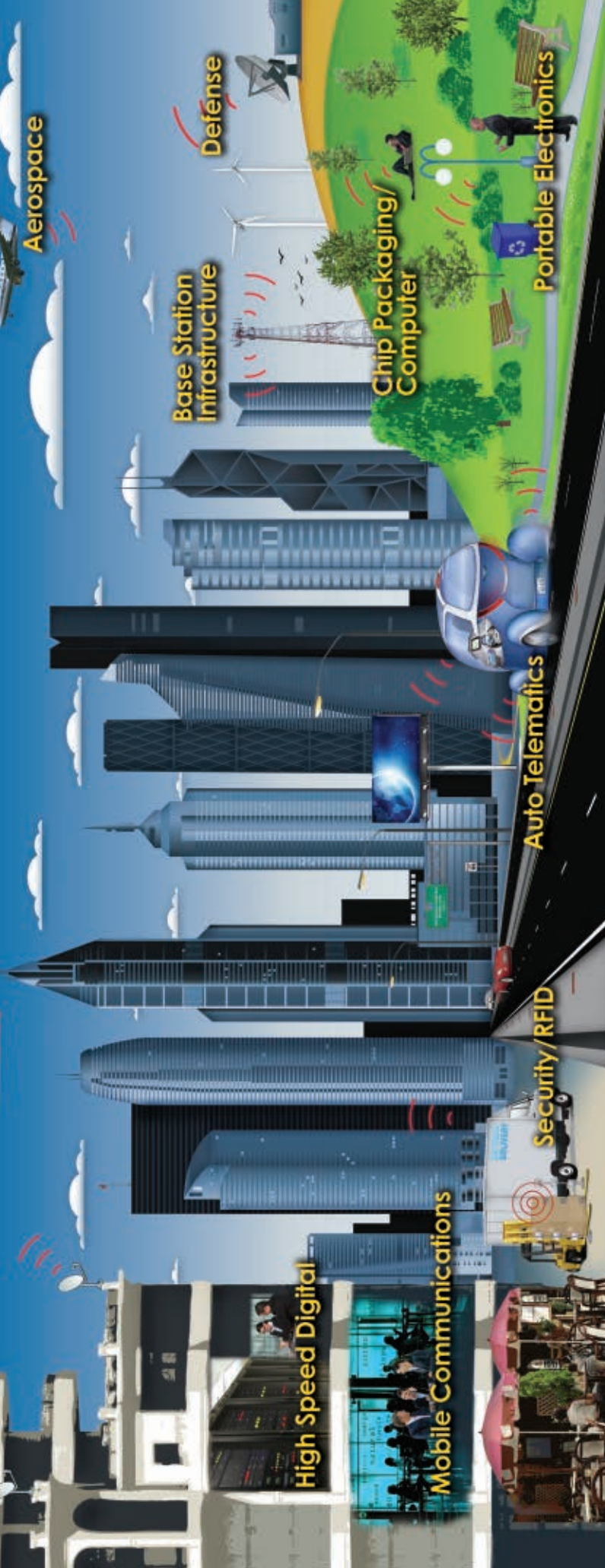
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SATELLITE COMMUNICATIONS DEVELOPMENT

The new satellite era dawned on 4th November 1957, when the first satellite, Sputnik-1, was launched by the USSR. From the very beginning, the use of satellites for military and commercial telecommunications was considered to be an important and promising application. Initial investigations were carried out both in the US and the USSR. The first experimental communications satellite SCORE, which stood for Signal Communications by Orbiting Relay Equipment, was launched in 1958.

Echo-1 satellite, a passive reflector realized as a 30 m balloon coated with aluminium and launched in 1960, was the first intercontinental satellite transmitting between stations in the US and Western Europe. However, Telstar-1, launched in 1962, was the first true communications satellite, with an active transponder working in C-band. This satellite was used to realize the first transmission of a TV signal between ground stations in the US and in Europe (the UK and France).

Because a satellite in low orbit moves above the Earth's surface, and many satellites are necessary to provide continuous services, the next step was to investigate the use of satellites placed in GEO. In 1964, Syncom-3 was the first geostationary communications satellite to be launched, which was used to transmit TV signals from the Summer Olympic Games in Tokyo, Japan.

In 1964, the International Telecommunications Satellite Organization (INTELSAT) was established as an inter-governmental organization with 12 participating countries, but the number of members grew rapidly over the next few years. The main task of this organization was to design, develop, construct, establish, maintain and operate the space segment of global commercial satellite systems.

In 1965, Early Bird (Intelsat-1) was the first commercial communication satellite launched in GEO, and the new era of commercial satellite communications began. Early Bird was 38.5 kg spin stabilized spacecraft with 2 transponders with the capacity of 240 telephone channels or one TV channel for point-point connections between ground stations placed in

the US and Europe. Due to the low power signal transmitted by the satellite, in the ground station, a very large parabolic antenna had to be used. In subsequent years, new generations of Intelsat satellites increased the number of available transponders.

At the same time the USSR developed its own satellite communications system to distribute TV programmes. Because a large part of the USSR territory lay in the polar region where GEO satellites cannot be operated, satellites placed in elliptical orbits were used—Molnia satellites.

The enormous growth in demand for satellite communications resulted in a plethora of operational satellites. In the 1970s, the regional satellite operators were established: INTERSPUTNIK for the USSR and Eastern Europe, and EUTELSAT for Western Europe. Also, the first national communications satellites were launched.

Technical developments of the 1970s and 1980s, which resulted in the increase of the satellite weight and supply power and the realization of low noise and high power microwave components, made it possible to use Ku-band and facilitate the significant reduction of antenna dimensions in the ground stations. Hence, the broadcasting of TV programmes, firstly to head-ends of cable television networks and then directly to individual users equipped with receiving terminals.

In 1991, SES ASTRA realized a new concept of collocation of many satellites in the same orbit position in order to increase the number of TV programmes accessible to the user without changing the orientation of the receiving antenna.

Digital transmission of TV programmes in the 1990s using the MPEG-2 compression standard was the next stage of development. It enabled the transmission of several digital programmes in the single transponder channel instead of one analogue programme, with comparable reception quality. This seriously increased the number of transmitted programmes available for the user.

With regards to the use of satellite communications to provide services for mobile users, 1979 saw the International Maritime Satellite Organiza-

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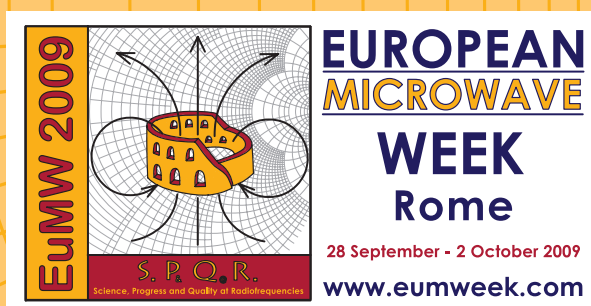
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tion (INMARSAT) established to realize communication with ships using GEO satellites operating in L-band.

At the beginning of the 1990s, investigations into the development of satellite mobile telephony systems were launched and specifically the use of constellations of satellites placed in Low Earth Orbit (LEO) and Medium Earth Orbit (MEO), in order to improve the power budget of the radio link between the satellite and handheld user terminal, in comparison with GEO satellites.

Two systems: IRIDIUM and GLOBALSTAR started commercial services in 1999 and 2000, respectively. However, these systems hit financial problems caused by the high cost of system development and short predicted life time in comparison to GEO systems plus a severe lack of user take-up. As a result, the implementation of other systems using LEO and MEO orbits were terminated.

This coincided with developments in satellite technology at the end of the 1990s whereby high power satellites with large deployable antennas could be built, meaning that mobile satellite telephony systems could be realized using GEO satellites. Thus, two systems—THURAYA and ACES—were built.

SATELLITE COMMUNICATIONS IN EUROPE

After the experimental tests of satellite communications in the US at the beginning of the 1960s, it was evident that telecommunications could be one of the most promising commercial applications of satellite systems. However, European activity was non-existent in comparison to the US and the USSR, and at the beginning of the satellite communication era, the European effort was virtually insignificant, being limited to the building of ground stations in the UK and France and then in Germany and Italy.

To change this situation, two major initiatives were instigated, namely international projects coordinated by the European Space Agency (ESA) and its predecessors, the European Space Research Organization (ESRO) and European Launcher Development Organization (ELDO) and national projects.

In 1967 ESRO began studies on the technical feasibility and economic

aspects of a European satellite communications system. It was deemed that going into competition with IN-TELSAT would be difficult so special applications for Europe were considered: intra-continental telephone connections (for the European Conference of Postal and Telecommunications Administrations - CEPT), distribution and exchange of TV programmes (for the European Broadcasting Union - EBU) and maritime communications.

In the early 1970s, a satellite communication system project was launched to consider the realization of an experimental satellite for the transmission of telephone calls and TV programmes [Orbital Test Satellite (OTS)] and a satellite for maritime communications [Maritime Orbital Test Satellite (MAROTS)].

At the same time, some countries started national or joint venture experimental communications satellite projects: SKYNET in the UK in cooperation with the US for military applications, SYMPHONY in Germany and France, and SIRIO in Italy. SYMPHONY-1, with two C-band transponders, was the first European communications satellite placed in GEO in 1974. In 1977, the ESA OTS-2 satellite was launched. This was the first communications satellite with Ku-band transponders capable of handling 7,200 telephone connections.

The first commercial European communications satellites were launched in 1981 [Maritime European Communication Satellite 1 (MARECS-1)] and in 1983 [European Communications Satellite 1 (ECS-1)]. MARECS-1 was the continuation and re-definition of the MAROT experimental programme and was used by INMARSAT. ECS-1 was the first of five satellites built by ESA and after the launch transferred to EUTELSAT as EUTELSAT I satellites.

In the 1980s and the 1990s, the next generations of EUTELSAT satellites, and also national communications satellites were launched, and European satellite communications began to play a significant role in the everyday life of citizens.

In the 1980s, the satellite broadcasting of TV programmes using telecommunications satellites with medium power transponders entered

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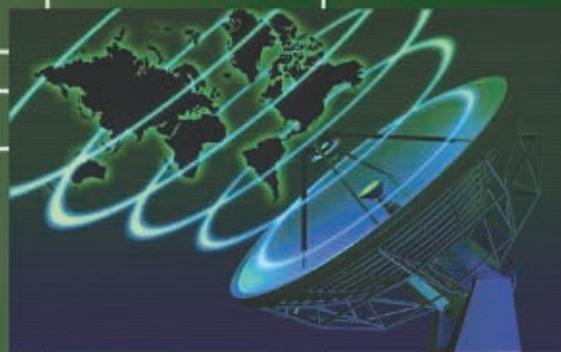
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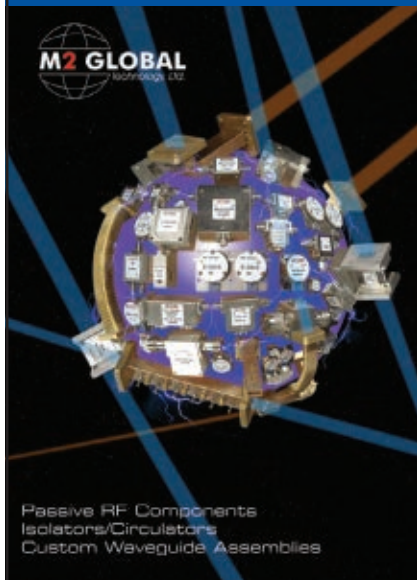
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Europe by the back-door, avoiding the decisions of WARC 77, with the use of high power Ku-band broadcasting satellites. Only a few broadcast satellites were launched and used, with the bulk of satellite TV programmes being transmitted using Ku-band transponders of telecommunication satellites. Increases in the number of satellites and the transponders they carried increased the volume of programmes available to users. In 1985, SES ASTRA, the first European private satellite operator in Europe, was established, launching the ASTRA-1 satellite and offering TV programmes to individual users, thus becoming a rival to EUTELSAT.

The great success of European satellite communications operators was connected to the broadcasting of digital TV programmes using DVB-S standards. The family of DVB standards were proposed by the European Broadcasting Union (EBU) and the European Telecommunications Standard Institute (ETSI) in 1995 to realize the transmission of digital television in different media (satellite, cable and then terrestrial) in Europe. Over the next few years DVB-S, based on the MPEG-2 compression method, became the worldwide standard. In 1996, satellite digital television based on this standard was launched in Europe, and now over 1,000 digital TV programmes and several hundred digital radio programmes are transmitted by ASTRA's satellites and EUTELSAT's HotBirds.

The DVB-S standard is also used for data transmission, i.e. realization of access to Internet via satellite, supported by a return channel realized by terrestrial telephone networks or by a satellite in Ka-band using the DVB-RCS standard.

In 2003, the next version of the DVB-S2 standard, based on the MPEG-4 image compression method, and adaptive spectrum effective modulation schemes was announced and implemented. Using this standard, a larger number of TV programmes can be transmitted in a single transponder channel. This transition to the digital television standard is related to the increasing number of programmes and the introduction of HDTV services in Europe. The DVB-SH standard relates

to the provision of multimedia data broadcasting services to mobile users.

As for the near future, the new satellite applications of interactive broadband transmissions, operating in S- and Ka-bands, will be offered to mobile and fixed users, respectively. Also, new satellites will be equipped with multi-beam antennas and advanced modern transponders operating at increased power levels.

MICROWAVE RADAR IN EUROPE: A HISTORICAL PERSPECTIVE

YVES BLANCHARD

Consulting engineer and author

When *Microwave Journal* was first published in July 1958, European electronics had scarcely recovered from the devastation of World War II. The industry needed to make up for lost time, be innovative and build on significant pre-war technological breakthroughs. These can be traced back to as early as the 1920s when European scientists were attracted by 'Ultra High Frequencies' and the unexplored world opening up beyond the 1 GHz border.

In 1923, Professor René Mesny went down to wavelengths of 1.2 m (250 MHz), and with his colleague, Pierre David, he organized a public demonstration of a radio link using such 'short' waves at the Physics and Wireless Telegraphy Exhibition in Paris, France. David had other applications in mind too, and as early as 1926 he started trials to detect airplanes by their electromagnetic radiation.

Next came Professor Heinrich Barkhausen of the Technical University of Dresden, Germany, who, with his colleague Kurz, reached the magical 30 cm limit with a triode fed in an unusual way: for their Positive Grid Tube they applied the high voltage to the grid instead of the traditional plate. This Barkhausen-Kurz oscillator is considered to be the first microwave oscillator.

In 1927, using a modified Barkhausen scheme, Professor Emile Pierret at the University of Nancy, France, reduced the wavelength to a new 12 cm record. During his tests he observed many effects of reflections in the cluttered yard of the faculty. Henri Gutton, a student who assisted him, would later remember these effects and deduce that a ship could be detected in this way. I shall

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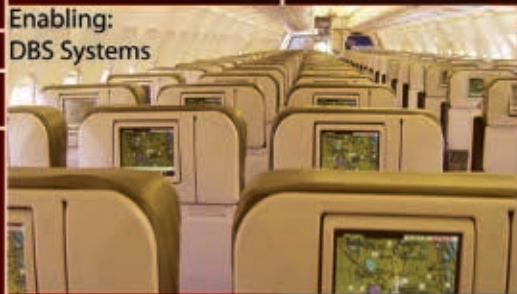
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explain later how he turned this idea into a radar reality.

The most spectacular achievement, however, was undoubtedly the link set up in 1931 across the Channel by an Anglo-French team from ITT, led by André Clavier. They demonstrated a focused beam—which they named a micro-ray—at 18 cm. Thus the advent of the European microwave pioneer was confirmed.

MAGNETRON: A EUROPEAN SUCCESS STORY

In 1904, the German Christian Hülsmeier failed in his project to provide shipping companies with his patented Telemobiloskop, which incidentally, could have saved the Titanic eight years later. For almost 30 years there were no significant microwave radar developments, all things being confined to the metric field due to the lack of sufficient powerful centimetric sources. However, in 1940 the definitive solution arrived in the form of the magnetron.

This valve had been envisaged in 1918 by the American A.W. Hull as a Lee de Forest's triode competitor, but it was not used as an RF source until 1924 when the Czech August Žačák and the German Erich Habann succeeded in bringing it into oscillation. In his Praha laboratory, Žačák got a 29 cm wave with a sort of Barkhausen mounting, and Habann took it one step further at the Jena University by suggesting that Barkhausen's negative resistance effect could be produced with a cylindrical fenced anode. This opened the way to a field of research that focused around three eminent European scientists: E.C.S. Megaw at GEC, UK, Klaas Posthumus at Philips NatLab, Netherlands, and Maurice Ponte at SFR-CSF, France.

Ponte began his magnetron research in 1932, with the aim of higher emitted levels and reduced magnetic fields. Pursuing Habann's idea he found that cutting the anode in multiple paired segments divided the magnetic field required by the number of segments. Over the next five years he continued his anode geometry trials with Henri Gutton. In 1937 they reached a peak power of 10 W at 16 cm with a tube they named M-16.

Ponte was in contact with Megaw who was mostly involved in the theo-

retical question of multi-modes coexistence in a given valve. He pursued this work in open competition with Posthumus, author of a new theory that he had named rotating field oscillations. Apart from their theoretical debates, Posthumus also set up a split anode magnetron that delivered about 10 W at 30 cm in 1933.

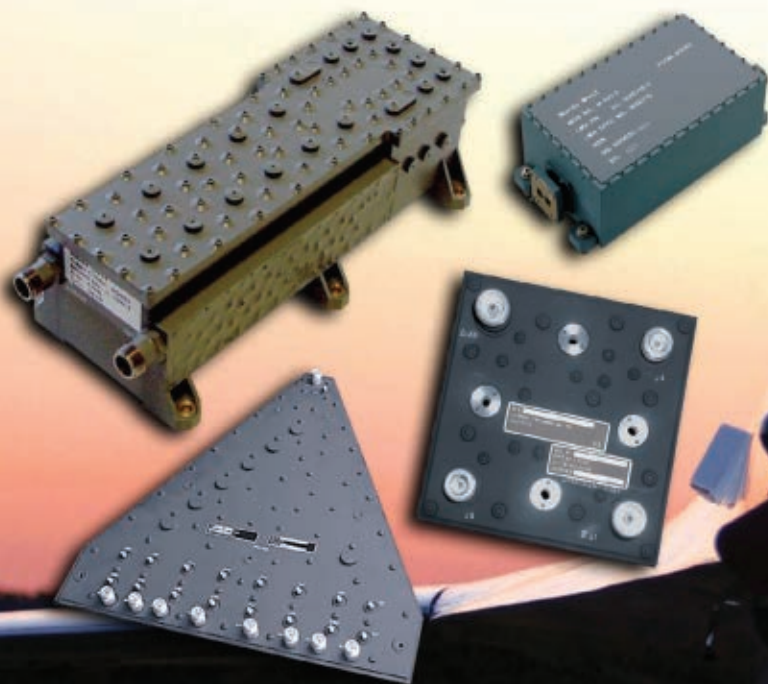
These 'first generation' magnetrons, despite their limited performance, found immediate applications as radar sources. In Germany in 1933 the trials for a naval radar by Rudolf Kühnhold used a Posthumus magnetron giving 40 W at 48 cm. In France, a decimetric radar (16 cm) was installed on board the liner Normandy by Gutton, first (1935) with a positive grid triode and later (1937) with his M-16 magnetron. In Holland in 1936 detection tests ordered to C.H. Staal by the Koninklijke Marine used a 10 W, 30 cm Philips magnetron. With the levels available, only large targets—civil liners or warships—could be considered for these attempts. All these research programmes proved the need for improved power sources.

It is well documented that, in England, Robert Watson-Watt had deliberately, and for a time successfully, excluded microwaves to set his Chain Home on a decametric basis. But when the enemy turned to bombing by night, Chain Home was not accurate enough to direct night-fighters within their interception range, and the need for efficient AI radars quickly resumed the interest in centimetric waves.

The decisive turnaround came from Professor John Randall and his student Henry Boot at Birmingham University, UK, who in 1939 had the bright idea to substitute cylindrical cavities in place of the external oscillating circuits of traditional magnetrons and to cut those cavities in a large copper ring used as the anode. On February 21, 1940, a six cavity prototype gave 400 W at 9.9 cm. Their next magnetron (E-1188), produced on May 16, was calibrated to give at least 1 kW.

Its only defect was a very short lifespan, due to the fast evaporation of the directly heated tungsten filament they used as the cathode. The last word lay with Ponte, who on May 9, 1940, only two days before the

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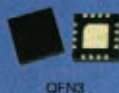


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German army broke through the front line and rushed to Paris, crossed the Channel with two samples of a new M-16 using an oxide coated and indirectly heated cathode. Bringing together the principles of the anode cavities and the oxide cathode, Megaw on June 26 achieved a 15 kW level, which exceeded all expectations. The cavity magnetron, disclosed three months later to the American allies by the Tizard mission, opened the way to the centimetric radar revolution, which was claimed to have changed the course of WWII.

POST-WAR EUROPEAN RADAR

Directly after WWII and for the next three decades, radar together with microwave radio links, supported the revival of the European microwave industry. British companies such as Marconi, GEC, Plessey and Ferranti had the privilege of priceless experience acquired during the war. In 1948 Marconi was charged with a study for the complete overhaul of the RAF radar chain round the whole of the UK. However, this favourable period was followed by two decades without any significant public orders. British companies, without major government procurements, struggled against US and new European competitors on the export market. The success of the privately-developed Martello in the 1980s came probably too late, when the dramatic restructuring of the European defence industry arose after the fall of the Berlin Wall.

In other countries, companies such as CFTH (France) or Microlambda (Italy) entered the field without any radar background, and chose to start on a US licensed basis. CFTH's first radars (a Precision Approach Radar, replica of the AN/MPN-1, and COTAL, a gun control radar issued from the SCR-584) were successful enough to give the company a solid position for markets of gun guidance (NATO Hawk programme, 1958); spatial trajectography (Aquitaine, 1955); and long-range 3D air surveillance systems. In 1963 CFTH won the NATO competition for equipping the NADGE long-range stations with its Palmier/ARES.

Microlambda opened in 1951 at Fusaro near Napoli in a pre-war tor-

pedo factory, as a joint venture between the Italian holding Finmeccanica and Raytheon, to start a radar production business. The first apparatus transferred to Fusaro was the TPS-1D. The successful completion of the contract opened the way for Microlambda to develop in an autonomous way. It became Selenia, which received the Italian part of the NATO Hawk programme.

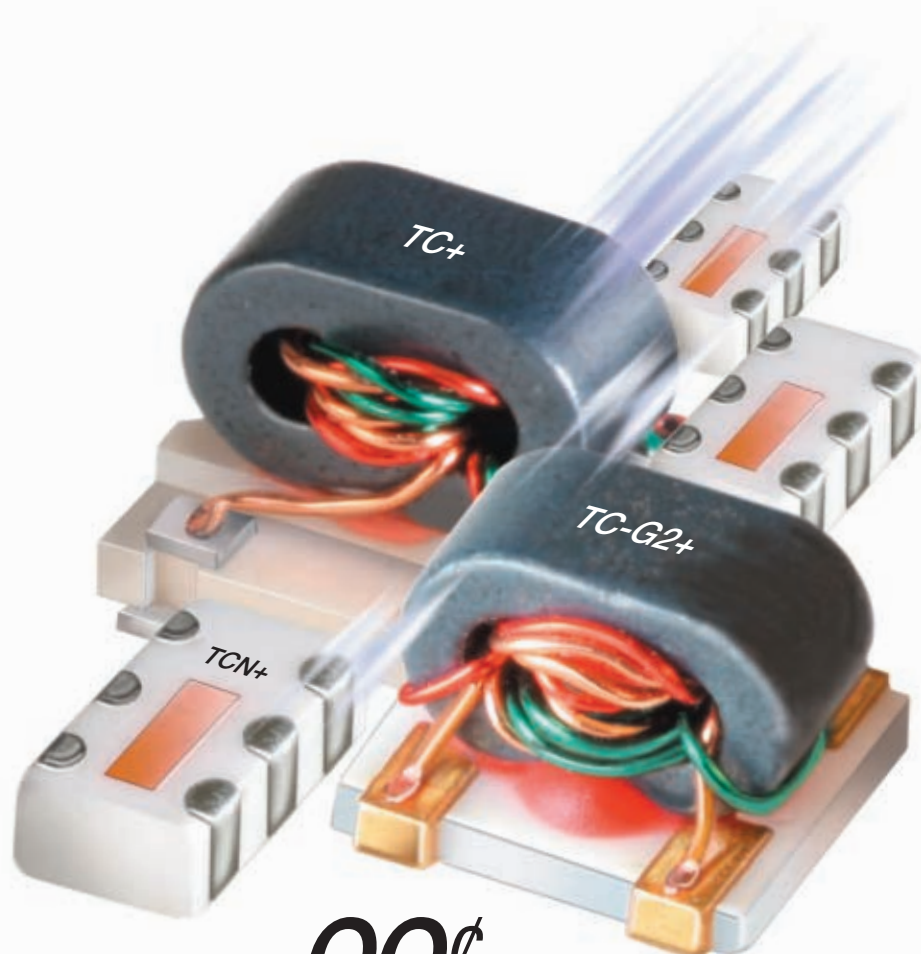
In the Netherlands Signaalapparaten (opened in 1922 at Hengelo) was a manufacturer of gun guidance systems. Captured by the Germans, and harshly damaged by allied raids, the factory reopened in 1945 to restart its original business. In the meantime radar had become a required element of Gun Laying systems. The task was given to Max Staal, who had installed, before the war, a 70 cm radar prototype on board the Dutch destroyer Isaac Sweers. As general manager of Signaal, Staal later produced a large range of successful radars for the Dutch Navy and for a worldwide export.

Named head of CSF, Ponte created a Radar Application Department in 1950 to take advantage of the pre-war experience of Gutton's decimetric radars, and acquired know-how in magnetron applications. CSF was the first to respond to French government requests for Naval radars, but its most significant success occurred in the airborne radar domain, after it won the bid for the fighter Mirage 3C radar with its famous Cyrano (1958), from which more than 1,000 sets were sold over the next 20 years.

For many years all these companies were confronted by the lack of microwave components, which they had to develop themselves, or buy from new specialist companies such as EEV in the UK. Until the mid 1960s progress in radar meant longer ranges (more powerful transmitters), and increased resolution (larger antennas). In 1957 CFTH achieved a world record with an S-band klystron delivering 30 MW peak power. This trend slowed down when advances in signal processing gave priority to wideband components. In 1968 the same CFTH laboratory succeeded in reaching a 10 percent bandwidth at 200 kW average power.

In the meantime, Doppler filtering and pulse compression had been

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RT233C	15	34	37	45	WP-22
RT240N	14	40	43	50	WQ-22
RT240C	14	40	43	50	WP-22
RT243N	12	43	45	52	WQ-12
RT243C	12	43	45	52	WP-12
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implemented. Pulse compression was patented during WWII by the German engineer E. Huttman (1940) but remained unapplied. In 1954, Charles E. Cook revived it at the US Sperry Co. for the AN/FPS35. It was not long before the idea came back to Europe: in March 1959, M.H. Carpentier at STTA, France, tested a laboratory model, which is said to be the second recorded in the world. In 1962 it was applied by CFTH to the experimental Conrad radar.

ACTIVE ANTENNAS: KEY TO THE NEW MULTI-FUNCTION SYSTEMS

In the '80s, R&D efforts considered the new concepts of phased arrays and electronic scanning, one major technical gap in radar development. It was not exactly a new idea, insofar as the WWII German Mammut was already an electronically scanned phased array. The concept was revived when size and weight of ABM early warning radars made mechanical scanning impracticable, and progressively it extended to complete radar families.

Three decades were necessary for making it technically workable, with two main ways of implementation:

- Passive Electronically Scanned Antennas (PESA) are powered by a single source sharing its output between many phase shifters plus transmitters modules. Power may be distributed to the radiating elements by a more or less complicated net of waveguide feeders, as implemented in the '80s French DRBJ11 or 22XX. In a more advanced architecture the power source may face an array of multiple phased reflectors (reflect array), or send its waves through an electronic lens. This solution, combined with a fast mechanical rotation, has been adopted both by Thales (Arabel) for the French SAAM anti-missile system and Selex (Empar) for the Horizon frigates PAAMS system.
- Active Electronically Scanned Antennas (AESA) feature the most advanced architecture. They use a large number of solid-state transmit/receive (T/R) modules, instead of the PESA single source. This improves beam agility and flexibility, saves energy and increases reliability. AESAs are specially suitable for multifunctional systems (to make a ground radar evolve from a general Air De-

fence mission to an extended Air and Missile Defence mission, for example.) First implementations were limited to an elevation '1D' e-scanning, with a classical rotating mode for azimuths: MASTER-A (Thales, 1995) or RAT-31DL (Selex, 1999) are both fitted with horizontal rows of radiating elements, fed with a vertical column of solid-state phase-controlled transmit amplifiers.

Getting full '2D' scanning required major investment. The UK Multi-function Electronically Scanned Adaptive Radar (MESAR) research programme was launched in 1982 jointly by Plessey and DERA. It resulted in an array of 1,264 elements, each delivering 10 W, quad-packed on a total of 316 T/R-modules. MESAR has initiated Sampson, an S-band Multi-Function Radar (MFR) produced by BAE Systems Insyte to be fitted to the PAAMS missile system of the Royal Navy's Type 45 destroyers.

Sampson's closest competitor is the Thales-NL X-band MFR Active Phased Array Radar (APAR), evolving from a Netherlands, Germany and Canada joint programme. As opposed to the Sampson's two rotating arrays, it uses a four array fixed structure.

Other projects have been in conjunction with US companies: Counter Battery Radar (COBRA) was a 1997 tripartite programme for equipping French, British and German armies with battlefield AESA C-band radar. It was developed in just two years by the Euro-ART (Advanced Radar Technology) consortium including Thales Air Defence, EADS Deutschland GmbH, Thales Defence Ltd., and Lockheed-Martin, which brought its T/R solid-state GaAs technology. Today Thales works in association with Raytheon in a 50/50 joint venture, Thales-Raytheon Systems, which develops the M3R project, a very flexible system with a fully modular architecture of octopacks (8 T/Rs).

Airborne radars are basically multifunction systems; ensuring air surveillance, air-to-ground and weapon control missions, and AESA should logically be the most suitable choice. But it has suffered for some time from the lack of mass-produced X-band T/R modules. The Airborne Multirole Solid-state Ac-

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OIP3 (dBm)	41	46	50	53	53	50
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RFC1G18H4-24	20~1000	36	46	DP-27
RFC1G18H4-24S	20~1000	36	46	SOT-115J
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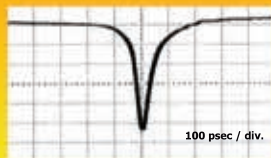
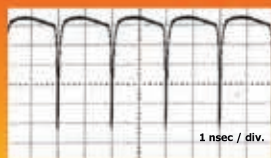
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GIM2000A	2000	-7	35

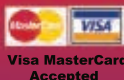
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tive Array (AMSAR) programme was launched in 1992 in order to set up a technology demonstrator within GTDAR [a consortium between Thomson-CSF, GEC-Marconi Avionics and Daimler Benz Aerospace (now EADS)]. This tripartite programme began in 2003 with flight trials beginning in 2008.

However, markets don't wait. To fit in with the Typhoon and Rafale fighter programmes, radar manufacturers had to provide interim solutions, respectively CAPTOR with a mechanical slotted antenna for the first, and RBE2 with an electronic lens PESA for the second. At the same time Thales studied a new 1000 T/R active antenna, based on AM-SAR experience, featuring a 'plug and play' antenna to be included in a new RBE2-AA. Simultaneously, a Euro-radar consortium, with Selex Sensors & Airborne Systems, Galileo Avionica—both united since May 2005 as Selex Galileo—EADS Defence Electronics, and INDRA made CAESAR, a 1425 T/R array to be plugged in an upgraded Captor-E CAESAR. AESA technology had become the de-facto standard for the radars of all advanced European fighters.

Technologically, active modules of an AESA are implemented with a limited number of monolithic integrated circuits, performing functions of phase shifter, microwave mixing, high power amplification, low noise amplification and T/R high frequency switching. More often HPA, LNA, attenuator and phase shifters use GaAs and the T/R switch uses a circulator. Today efforts lay in packaging, cooling, and compatibility with 'tile' antenna architectures. In the next five years, new components like GaN (which support higher power density and wider bandwidth) should be introduced for HPA and LNA, SiGe for phase shifters, and MEMS for power switching.

Providing radar manufacturers with adequate AESA components has become a top priority for the European microwave industry. It is a good opportunity to enforce Europe's position in the highly competitive market of GaAs and other MMIC technologies. In return, radar should benefit to some extent from the mass production techniques developed for the consumer electronics market.

CONCLUSION

This Report began by relating the state of the European microwave industry in the early 1960s and posed questions as to how it had changed and developed during the intervening years. Of course, there are no definitive answers apart from the fact that the continent has had to adapt to political change, particularly in Eastern Europe and the expansion of the EU, economic pressures and competition from emerging markets such as India and China.

A stark reality is that against the background of changing markets and increased competition, companies have undergone rationalisation, merged or made acquisitions. In recent years the landscape of European microwave companies has changed with many of the household names that were synonymous with the industry being renamed, merged or gone completely. Now, companies are rarely single country flagships, but more likely part of large international organisations.

However, what has not changed and what has been illustrated in this Report is the wealth of industrial and academic expertise that is not only a part of Europe's history, but is also its present and its future. Europe is at the forefront of technological development in many sectors. Through Europe-wide initiatives such as the Framework Programme (now in its 7th stage) and the associated Networks of Excellence Programmes, microwave research is taking an interdisciplinary and collaborative approach enabling system capabilities to guide the selection of new technologies. This is being backed up with financial investment and commercial development in an environment of coordination and cooperation at academic, industrial and political levels. Europe has a rich and valuable microwave history. That can continue if it focuses on exploiting its core competencies of a highly skilled research and development capability and the production of added value products and services. ■

ACKNOWLEDGMENTS

The author would like to thank Józef Modelski and Yves Blanchard for their time and effort, and for sharing their knowledge and expertise.

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AP1053	10-1000	11.0	1.5	26.0	97	39/58	15	100
ARJ109	0.5-200	10.8	4.5	28.5	96	44/75	15	235
AR1096	600-1000	14.2	2.1	28.0	96	42/58	15	230
AP348	10-250	13.5	3.2	25.0	95	42/57	15	108
AP2009	10-2000	11.0	3.5	28.0	95	40/50	15	188
AP1051	10-1000	11.5	1.5	23.0	94	35/52	8	89
AP2079	10-2000	10.3	3.1	24.5	94	38/54	15	125
AC652	10-600	10.8	1.3	18.8	93	32/45	5	48.5
A2CP6008	2000-6000	11.0	3.0	24.0	92	34/50	12	250
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A MICROWAVE JOURNEY, PART IV: THE 1980s

This six-part series looks at five decades of the microwave industry recorded in *Microwave Journal*. In this fourth installment, we focus on the 1980s, a decade marked by such notable events as the birth of MTV, punk rock and “new wave,” the marriage of Prince Charles and Diana, the Cosby Show, the fall of the Berlin Wall and disasters such as the bombing of Flight 103 over Lockerbie, Scotland, the Challenger explosion, and industrial accidents at a chemical plant in India and a nuclear facility at Chernobyl in the former USSR.

The decade also saw dramatic social, economic and political change. Economic liberalization among western countries came with the rise of right-wing politics in the US and the “Reagan Revolution” along with other world leaders such as Margaret Thatcher, Helmut Kohl, Brian Mulroney and Carlos Salinas. Among eastern countries, hostility toward authoritarianism put pressure on the economies of communist states, bringing about policies such as perestroika and glasnost, while developing countries felt the crushing economic burdens brought on by a debt crises, drought, food shortages and war.

During the Reagan years, the Cold War would heat-up and spawn renewed investment in the US military with a particular focus on R&D. Once again, the microwave industry was a beneficiary of this government spending. The money led to significant advances for microwave components used in EW, ECM, guided tactical weapons, and tactical communications systems for command and control architecture. Commercially, the huge demand for voice and data transmission led to major advances in digital modulation techniques, satellite communication continued to advance, providing links for the distribution of content to local cable TV operators. GaAs and MMIC technology, driven by the needs of the military experienced great technical gains, yet also experienced a disastrous start in the commercial world and test & measurement showed significant advances due to microprocessors while computer aided design moved from the research lab to the microwave designer, aided by the personal computer.

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150-70	dc-18.0	0-70/10		3200-1E-2	dc-3.0	0-127/1	
150-70-1	dc-18.0	0-70/10		3200-2E-2	dc-3.0	0-63.75/.25	
151-11	dc-4.0	0-11/1		3201-1	dc-2.0	0-31/1	
152-90-3	dc-26.5	0-90/10		3201-2	dc-2.0	0-120/10	
150T-11	dc-18.0	0-11/1	◆	3206-1	dc-2.0	0-63/1	
150T-15	dc-18.0	0-15/1	◆	3200T-1	dc-2.0	0-127/1	◆
150T-31	dc-18.0	0-31/1	◆	3206T-1	dc-2.0	0-63/1	◆ X
150T-62	dc-18.0	0-62/2	◆	3250T-63	dc-1.0	0-63/1	◆ X
150T-70	dc-18.0	0-70/10	◆	3406-55	dc-6.0	0-55/1	New
150T-75	dc-18.0	0-75/5	◆	3408-55.75	dc-6.0	0-55.75/0.25	New
150T-110	dc-18.0	0-110/10	◆	3408-103	dc-6.0	0-103/1	New
151T-110	dc-4.0	0-110/10	◆	4216-63	0.8-3.0	0-63/1	
152T-55	dc-26.5	0-55/5		4218-127	0.8-3.0	0-127/1	
153-70	dc-40	0-70/10	New	4238-103	.01-2.5	0-103/1	
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THE 1980S February 1980

While the first issue of the new decade may have included a broader range of application topics (e.g. "Microwave Communications from the Outer Planets: The Voyager Project;" "A Rotating Directional Antenna Feed System for a Microwave Oven;" "Microwave Apparatus for the Treatment of Cancer by Hyperthermia;" and "A Synthesized Approach to Satellite-TV Reception"), February was focused on defense electronics. In a special report, Lynwood Cosby of Naval Research Labs wrote about the microwave challenges for EW applications in the '80s. His two principle observations were that "A broad technology base must consistently exist to support the wide range of equipment development options." The author described several past wartime events where a gap in electronic technology between combatants significantly influenced the outcome. He cautioned readers that "We must not fall in the trap of believing that EW is a mature technology." The author's other main observation (and by his accord—even greater significance) was that "it is better to take a high-risk long-shot R&D approach rather than stay with a tried and proven approach." Again the author used examples from history to lobby for what we frequently refer to now as "disruptive" technology. In presenting his case for taking a high risk approach to component design for EW, the author explicitly mentions solid-state technology. The defense department's interest in solid-state technology and GaAs devices in particular is evident in numerous articles appearing in this issue and others throughout the '80s.

Other defense related articles this month included a special report on the 1979 DoD/AOC (Association of Old Crows) EW Symposium, Principles of EW: Radar and EW; and a look at Navy Microwave Component Contracts by Eliot Cohen of NRL. The author looked specifically at contract programs to develop S-band power GaAs FETs, FET amplifiers (including low noise amplifiers), Schottky barrier mixer diodes (for use in 94 GHz systems) and monolithic integrated circuits. Contract winners

SPECIAL REPORT

mentioned by name included Avantek, Hughes Aircraft, Microwave Associates and Texas Instruments.

March 1980

Either by intent or coincidence, the following month was dedicated to the theme of microwave solid-state. In the guest editorial, "The First Thirty Years" by Lawrence Thielen of AvanteK, the author congratulated *Microwave Journal* founder William Bazzay for predicting that "the microwave industry would come of age at the dawning of the '80s." The author cited the yearly revenue of the average mid-sized microwave component manufacturer and the value of a typical contract and concluded that the industry was too prosperous for the investment community to ignore. "These investors have come to realize that our once-fledgling cottage industry—largely DoD supported—is today an industry with great depth and breadth, and one with remarkable growth potential and staying power." Another interesting comment from the author of this article, nearly 30 years old: "Our technology is even helping to reduce the debilitating effects of high-priced petro-energy—inexpensive, effective communications eliminates the need for many auto and airline trips."

Theme-related articles included a special report from Keith Kennedy of Watkins-Johnson on the then recent technical advances and projections for continued improvements to microwave and millimeter-wave solid-state devices. Seeing solid-state as critical to reducing costs and forcing standardization, the author specifically called attention to advances in Gunn and IMPATT diode technology. Taking more of the spotlight than these two device types was the GaAs MESFET. Fellow W-J engineer, Karl Niclas wrote a technical article on GaAs MESFET feedback amplifiers. Ira Drukier of Microwave Semiconductor Corp. (MSC) discussed the "Design of a 15 GHz High Power GaAs FET." The performance of this device from the early '80s showed a peak output power of 30 dBm, 6.7 dB gain at 17.0 percent PAE. Raytheon technical guru and author of microwave device text books, Robert Pucell wrote an article entitled "Per-

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formance of GaAs MESFET Power Combiner" in which he described a four FET combiner that delivers over 2 W of output power at 10 GHz. Meanwhile, contributing editor Joseph White wrote a special report entitled "Why Go to MTT?"

May 1980

Microwave Journal dedicated its May issue to the MTT-S Symposium with the magazine cover showing the conference location (Washington, DC). The magazine included a listing of the complete technical guide and exhibitor list, and map of the exhibition floor plan. Editor Joseph White wrote the second of *Microwave Journal's* annual "Attending the Conference" article. The format of the "show issue" and our extensive coverage began the year before in April 1979 and will go mostly unchanged right through today. Starting in 1980, however, the show issue is published every May up to the present.

January 1983

The January issue is dedicated to communication systems and featured articles describing an industry grappling with how to improve the capacity and efficiency of voice and data transmission. While cell phone technology is not among the challenges mentioned, the digital modulation techniques that will make cell phones feasible are the focus of several articles. The communication systems written about were concerned with applications such as common-carrier digital point-to-point terrestrial radios for long haul telecommunications, satellite relay links, privately owned digital switches and microwave links for industry and point-to-multipoint inter-city communication networks to mention a few.

By 1983, digital technology was being heavily investigated by the microwave world, made evident in a business/special report by guest editor Harold Sobol of Rockwell International (Collins Transmission Systems Division). In his article, "Progress in Microwave Communication Systems," Sobol brings the reader up to speed on the state-of-the-art in communications equipment. "Digital radios for PCM voice and data transmission, interconnections of

electronic digital switches and wide-band encrypted messages have been in service during the last five years," wrote Sobol. "Earth stations for satellite relay stations are undergoing enormous changes and direct broadcast video systems for residential use are just around the corner."

Sobol described the primary factors responsible for changing microwave communications equipment to be "the growth of telecommunications in the public, private and government sectors and the demand for new types of service." The goal then (and now) was to increase channel capacity within FCC allocated channels. Sobol wrote about analog long haul FM radios (6 GHz, 30 MHz BW, 2700 voice circuit capacity per channel) being replaced with SSB radios with 6000 voice circuit capacity (a significant improvement in spectrum utilization), the capacity of high density microwave digital radios (employing 8 PSK, 16 and 64 QAM modulation schemes) and the promise of fiber optics to address the channel capacity challenge. At the time of this editorial, new digital radio technology based on 64 QAM showed an increase in capacity of 50 percent at 6 GHz compared to the 8 PSK radios, which was the modulation technique in the majority of digital radios in use at the time. This put 64 QAM on par with analog FM, but still a far cry from the analog SSB radios.

May 1983

The Boston skyline at dusk graces the cover of the *Journal* in honor of the location of MTT-S in 1983. That year's conference was projected to be the largest to date with 250+ exhibitors (an increase of 25 percent over the previous high). Guest Editorial included MTT-S Adcom president Charlie Rucker who wrote about the engineer supply problem. Technical Program Chair Ralph Levy and Consulting Editor Joe White who was also serving as Chair of Special Events wrote pre-show articles. Future *Microwave Journal* publisher/editor Harlan Howe served as the chairman of that year's Steering Committee.

It was also a big year for microwave instrumentation equipment to appear on *Microwave Journal* covers, reflecting the developments oc-

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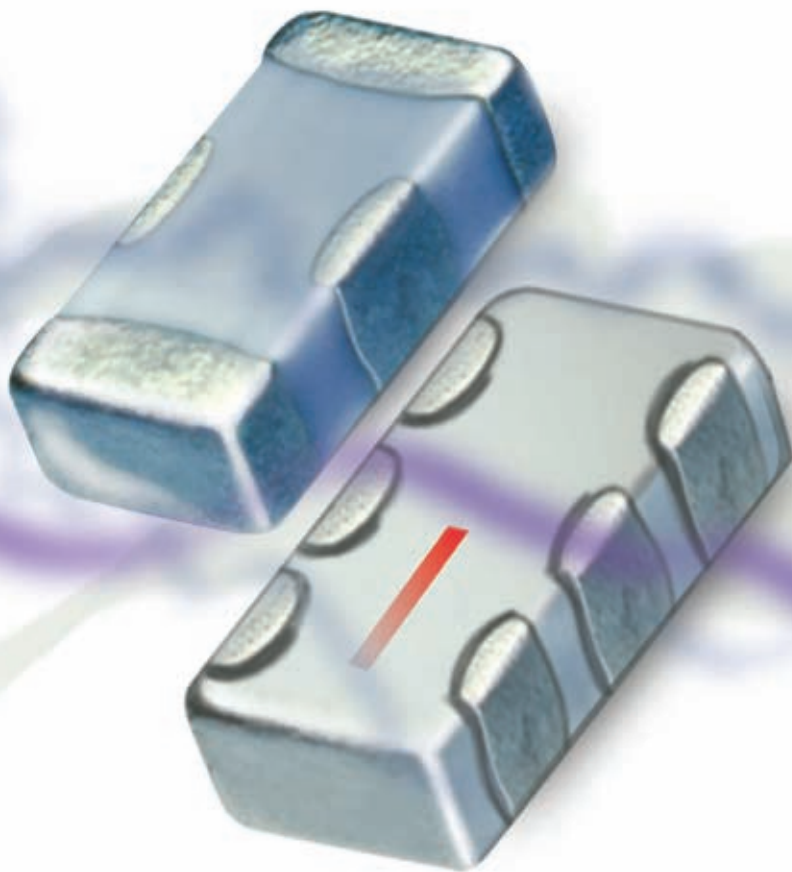
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curing in the automation of test & measurement systems. These new capabilities were made possible in part through the recent advances in microprocessors. A fourth generation Hewlett-Packard scalar network analyzer was featured on the cover of March's "microelectronics" issue, Wiltron's 5669 ANA with a measurement sweep range up to 40 GHz was featured on the cover of the June "millimeter-wave" issue, a Marconi power meter that "exploits microprocessor capabilities to enhance the speed and accuracy of its average and peak power measurements" appeared on the April "microwave instrumentation" issue, another power meter appears on the November "super-components" issue (this time the "new" 438A dual sensor power meter from HP) and in December, a photo of a Wavetek model 952 1 to 4 GHz microwave source. This focus on instrumentation on the cover spills over into 1984 with the January cover featuring the new vector "real-time" network analyzer also from HP.

January 1988

Digital communication is again the focus of the January issue and in the five years since the editorial by Sobol, Ferdo Ivanek of Communications Research reports that the effort to match and eventually surpass the spectral efficiency of SSB via digital radio is about half the way to its goal with a system using 256 QAM (not yet in commercial operation). However, work is already under way to double the spectral efficiency through frequency re-use with orthogonal polarizations. The gap continued to close between analog and digital radios.

The author mentioned that achieving greater spectral efficiency would come at the cost of system complexity, which in turn would require higher-levels of circuit integration. At the time, high level integration was beyond the state-of-the-art for GaAs MMICs, but was well within the reach of CMOS. An additional challenge for multilevel modulation methods used by these digital radios was the serious performance degradation of nearly saturated solid-state power amplifiers due to nonlinear behavior. The hope of achieving greater

capacity through digital modulation would depend on advances in developing RF integrated circuit technology. Of the other papers that month addressing digital microwave communications, three are system related dealing with high capacity transmission using 16 QAM, 64 QAM and 256 QAM, and the other two are on microwave components—power amplifiers and oscillators.

Several times that year, the state of GaAs technology and the GaAs market comes under scrutiny. The first article dealing with this topic is "The Elusive GaAs MMIC Market" by Jeff Montgomery of ElectroniCast Corp. Since Frank Brand wrote in *Microwave Journal* 10 years earlier that the promise of GaAs could be threatened by a shortage of material suppliers, 30 laboratories worldwide had made major investments in the technology (partially with US government support). Investments of \$91 M in 1987 were expected to reach \$194 M by 1992 in pursuit of business projected to be within the range of \$500 M to over a \$1 B by 1991. Nice return. Unfortunately, at the time of this article, the author reported that the enthusiasm of almost every laboratory manager was in decline as they were beginning to conclude that high volume use of GaAs MMIC was much further out than originally projected. Why? The earlier studies were based on the consensus views of the researchers themselves rather than the markets they would be selling into. Because most labs were captive, MMIC researchers and manufacturers could not see past their own needs. The importance of high volume production and low cost was initially off everyone's radar.

A similar outlook was shared by editor Joe White in his April article "GaAs: The Bumpy Road." White wrote that the market for GaAs devices could be met by two firms; the remainder represented manufacturing overcapacity. Still, speed performance including that of the relatively new HEMT devices fueled the remaining optimism for the technology. Various individuals provided their predictions as to who would succeed and who would fail. Some would re-coup their investment by offering foundry services

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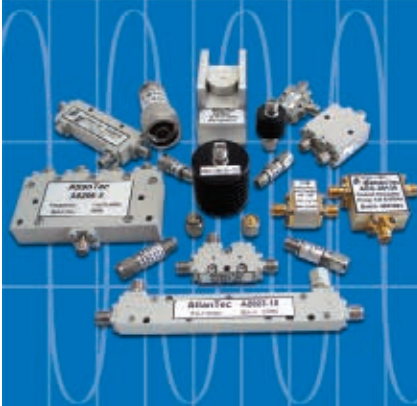
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offering MMIC circuit realization (three to five wafer execution over six months at a cost between \$50,000 and \$100,000) while others would succeed by finding the right niche markets best suited for the benefits of GaAs devices and not hampered by any technical or production-related downside. The losers would likely be captive fabs with only a military customer to cover their expenses.

Nineteen eighty-eight saw new activity on the computer simulation front with an ad from Compact Software depicting a new nonlinear simulator for microwave frequencies based on a technique known as harmonic balance. The simulator called Microwave Harmonica is portrayed as a race car, speeding past another race car labeled SPICE. Microwave Harmonica would be the cover story ("New Design Workstation Simplifies the Design Process") of the July issue that year. EEsof, which introduced the PC platform-based Touchstone circuit design product in 1983, introduced Omnisys. This simulator specifically for microwave system designers made its *Journal* debut as an insert in the May Show issue and in a technical feature that month. Hewlett Packard (now Agilent) would acquire EEsof to complement its design software product called Microwave Design System (MDS) and eventually both products would be replaced by the familiar ADS product still in use today.

January 1989

In the first issue closing out the decade, *Microwave Journal* Staff Editors Martin Stiglitz and Lloyd Resnick provided a report on the government program that, unlike any other, tied together all the advances in solid-state processing and design development, test and measurement techniques and computer-aided design and would propel these technologies to the next level. Their article—"The MIMIC Program: A Technology Impact Report"—gave an excerpt on the MIMIC program, including its goals, structure, program phases, and the targeted military and commercial applications. This program epitomized the convergence of technical advances that took place over this phenomenal

SPECIAL REPORT

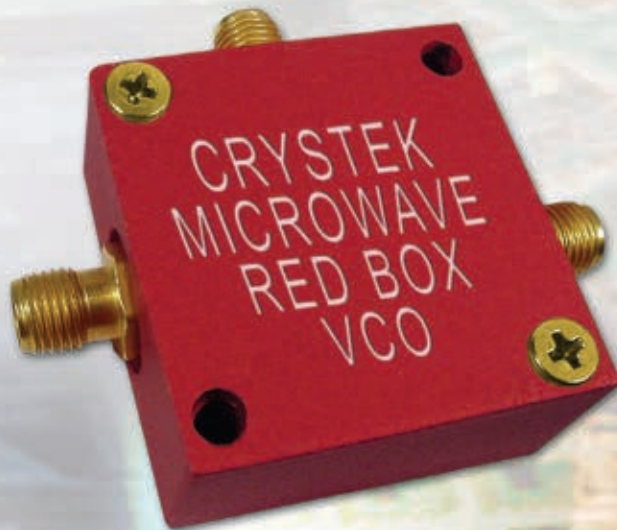
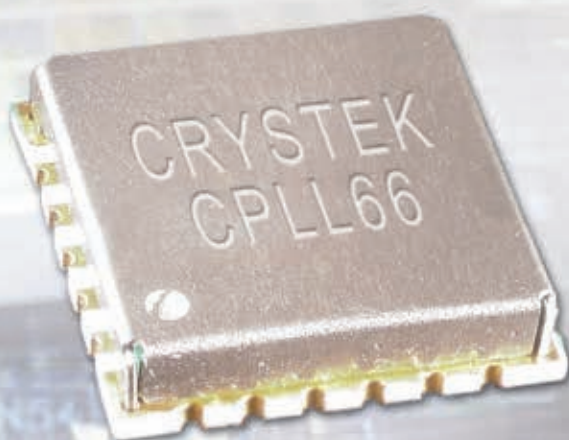
decade in microwave technology. MIMIC was a R&D effort sponsored by the DoD and conducted by DARPA and the military services. Together, they would be responsible for developing a family of monolithic analog integrated circuits and modules that could be used in the front-end of military electronic systems operating at microwave or mm-wave frequencies.

The program was modeled after the very high-speed IC (VHSIC) program and would be largely responsible for inter-company cooperation and technical developments that would not likely be pursued by civilian companies because of the limited commercial potential. However, the resulting advances would create new markets and opportunities similar to those created by the development of the Internet (another DARPA project). It is hard to imagine how today's mobile communication would have been possible without the influence of this program. It may also be equally hard to find a microwave engineer over the age of 40 who was not somehow connected to this program directly.

CONCLUSION

Driven by social and political activity, which was responsible for increased investment in military R&D, significant advances in solid-state processing and design for RF/microwave devices, modules and integrated circuits took place. Along with high-frequency device technology, advances in digital ICs provided the technology that would forever change the capabilities of test & measurement equipment and the computers that would host the new computer-aided design software that was becoming more abundant for microwave design. The industry would also be focused on developing methods to improve spectral efficiency to address the growing demand for data transmission. All these developments of the 1980s and the ending of the Cold War would provide the perfect alignment of resources, technology and need for new markets that would help our industry take on and achieve commercial success of an unprecedented scale—the wireless revolution of the 1990s. ■

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AN APPROACH FOR DETERMINING MOSFET SMALL-SIGNAL CIRCUIT MODEL PARAMETERS

A simple method for the extraction of the small-signal model parameters of a MOSFET is proposed. The intrinsic elements determined are described as functions of the extrinsic resistances. The parasitic elements are iteratively determined using the variance of the intrinsic elements as an optimization criterion. Good agreement is obtained between simulated and measured results over a wide range of bias points up to 30 GHz.

For the fabrication of high-performance CMOS RF/microwave IC modules, suitable IC design and device characterization technologies for high-frequency applications should be well established. A critical issue in the technologies is the development of a physically acceptable small-signal MOSFET model and an accurate parameter extraction technique, which are crucial to design linear RF ICs such as low noise amplifiers and develop a large-signal model for nonlinear RF IC design. In addition, this small-signal modeling is increasingly important because the device characteristic data used for optimizing RF device performance during the development cycle of process integration can be provided

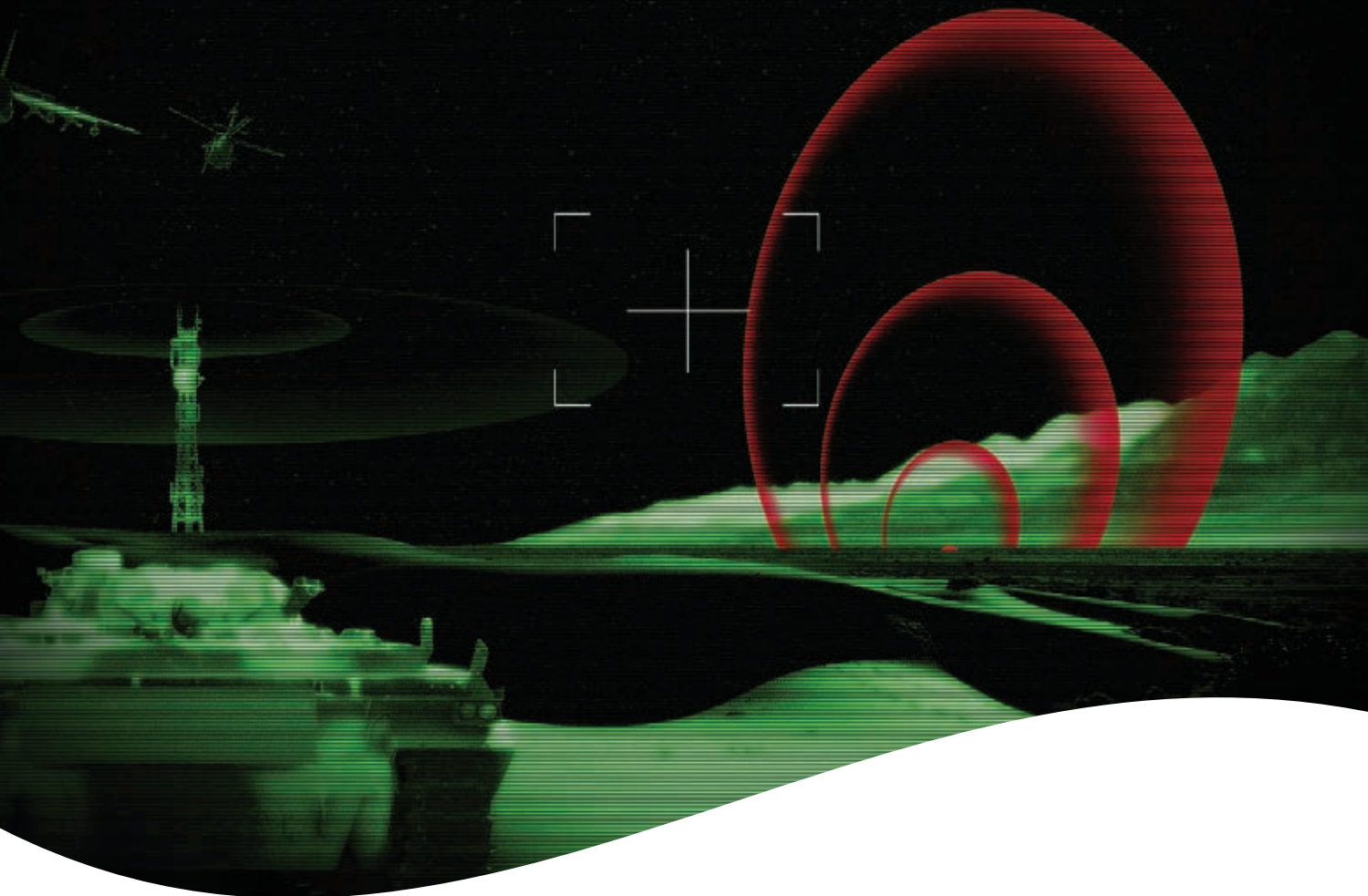
through the extraction of small-signal model parameters.¹

An accurate procedure for extraction of the extrinsic resistances is extremely important for silicon MOSFETs. Optimization methods have conventionally been used for the determination of these parameters. However, the accuracy of the numerical optimization methods that minimizes the difference between measured and modeled S-parameters versus frequency can vary, depending upon the optimization method and starting values, and may result in nonphysical and no unique results for the extracted elements.² For the direct extraction of small-signal MESFET equivalent circuits from S-parameters, parasitic inductances and resistances are initially determined and subsequently the rest of the parameters are extracted from formulations.^{3,4} However, this

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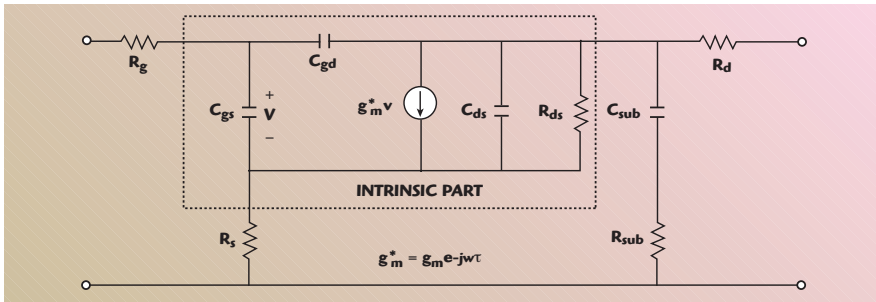
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▲ Fig. 1 Equivalent circuit of a MOSFET.

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cold-FET method cannot be applied to extract these resistances for Si MOSFETs because the DC gate current cannot flow due to the isolation between the gate and the rest of device. As a modified approach⁵ for Si MOSFETs, extrinsic resistances have been extracted from S-parameters at zero bias condition ($V_{GS} = V_{DS} = 0$). This method may produce uncertainties due to possible bias dependences in the extraction of source and drain resistances.⁶ Because of these difficulties, the values of the extrinsic resistances are often guessed or set to zero.⁷

In this article, an improved method to determine a MOSFET equivalent circuit, including the substrate-related parameters, is proposed. This method combines the advantages of the analytical and optimization extraction methods, and extracted results that are more accurate can be obtained. The intrinsic elements determined are expressed as functions of the extrinsic resistances. Assuming that the equivalent circuit is valid over the whole frequency range of the measurement, the parasitic elements are iteratively determined using the variance of the intrinsic elements as an optimization criterion.

ANALYTICAL DETERMINATION OF THE EQUIVALENT CIRCUIT

Parameters Extraction

Figure 1 shows the equivalent circuit of a short-channel MOSFET, whose intrinsic behavior is properly modeled by means of a quasi-static (QS) approach. Once the extrinsic resistances are determined, the intrinsic elements can be determined after de-embedding the open and short structures by using four steps as follows:

- 1) Subtraction of R_g and R_d :

$$Z_1 = Z_{DUT} - \begin{bmatrix} R_g & 0 \\ 0 & R_d \end{bmatrix} \quad (1)$$

Where Z_{DUT} is the matrix obtained from conversion of the de-embedded S-parameters to the corresponding Z-parameters.

- 2) Subtraction of the substrate parasitics:



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$$\begin{bmatrix} 0 & \omega^2 C_{jd}^2 R_b & 0 \\ 0 & \frac{\omega^2 C_{jd}^2 R_b}{1 + \omega^2 C_{jd}^2 R_b^2} + \frac{j\omega C_{jd}}{1 + \omega^2 C_{jd}^2 R_b^2} \end{bmatrix} \quad (2)$$

For the case of the substrate elements (R_{sub} and C_{sub}), the extraction is also biased on the MOSFET's equivalent circuit model at $V_{ds} = V_{gs}$

= 0.8 The real part of $1/Z_{22}$ at $V_{ds} = V_{gs} = 0$ is given by

$$\frac{\omega^2}{\text{Re}(1/Z_{22})} = R_{sub}\omega^2 + \frac{1}{C_{sub}^2 R_{sub}} \quad (3)$$

R_{sub} can be determined from the slope m_0 of the linear regression of the $\omega^2/\text{Re}(1/Z_{22})$ versus ω^2 data,

whereas C_{sub} is determined from the intercept with the abscissa b_0 by applying:

$$C_{sub} = \frac{1}{\sqrt{m_0 \times b_0}} \quad (4)$$

3) Subtraction of R_s :

$$Y_3 = (Y_2^{-1} - \begin{bmatrix} R_s & R_s \\ R_s & R_s \end{bmatrix})^{-1} = \begin{bmatrix} Y_{11} & Y_{12} \\ Y_{21} & Y_{22} \end{bmatrix} = \begin{bmatrix} j\omega(C_{gs} + C_{gd}) & -j\omega C_{gd} \\ g_m e^{j\omega\tau} - j\omega C_{gd} & R_{ds}^{-1} + j\omega(C_{gd} + C_{ds}) \end{bmatrix} \quad (5)$$

4) Intrinsic Elements

The intrinsic elements can be obtained from the intrinsic Y-parameters.

$$C_{gd} = -\frac{\text{Im}(Y_{12})}{\omega} \quad (6)$$

$$C_{gs} = \frac{\text{Im}(Y_{11}) + \text{Im}(Y_{12})}{\omega} \quad (7)$$

$$C_{ds} = \frac{\text{Im}(Y_{12}) + \text{Im}(Y_{22})}{\omega} \quad (8)$$

$$R_{ds} = -\frac{1}{\text{Re}(Y_{22})} \quad (9)$$

$$g_m = |\text{Im}(Y_{21}) - \text{Im}(Y_{12})| \quad (10)$$

$$\tau = -\frac{1}{\omega} \tan^{-1}(\text{Im}(Y_{21}) - \text{Im}(Y_{12}), \text{Re}(Y_{21}) - \text{Re}(Y_{12})) \quad (11)$$

CRITERION OF CIRCUIT VALIDITY

The intrinsic elements can be determined by solving Equations 6 to 11 as functions of the extrinsic elements as well as frequency:

$$R_{sub} = f_0(\omega, R_g, R_d, R_s) \quad (12)$$

$$C_{sub} = f_1(\omega, R_g, R_d, R_s) \quad (13)$$

$$C_{gd} = f_2(\omega, R_g, R_d, R_s) \quad (14)$$

$$C_{gs} = f_3(\omega, R_g, R_d, R_s) \quad (15)$$

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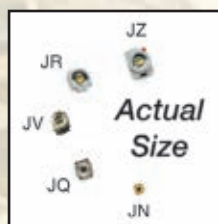
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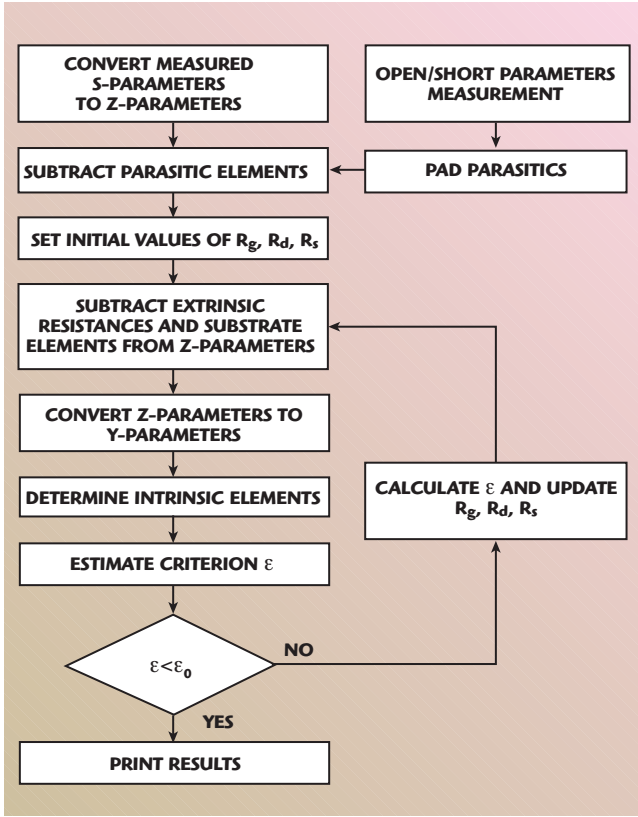
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▲ Fig. 2 Flow chart of the iterative process.

$$C_{ds} = f_4(\omega_i, R_g, R_d, R_s) \quad (16)$$

$$R_{ds} = f_5(\omega_i, R_g, R_d, R_s) \quad (17)$$

$$g_m = f_6(\omega_i, R_g, R_d, R_s) \quad (18)$$

$$\tau_m = f_7(\omega_i, R_g, R_d, R_s) \quad (19)$$

where ω is the angular frequency and $I (=0, 1 \dots N-1)$ is the number of sampling points.

Assuming that the equivalent circuit is valid for all frequency measurement points and making use of the intrinsic elements for optimization criteria, the appropriate values for extrinsic elements can be determined by iteration without complicated additional measurements.

The first candidates for criteria are the derivatives of intrinsic elements with respect to frequency, but they sometimes suffer from numerical and measurement errors. Therefore, variances are chosen as criteria.⁹ That is:

$$\epsilon_1^k = \frac{1}{N-1} \bullet \sum_{i=0}^{N-1} \left| f_k(\omega_i, R_g, R_d, R_s) - \overline{f_k(\omega_i, R_g, R_d, R_s)} \right|^2 \quad (20)$$

(k = 0, 1, ..., 7)

Moreover, for stable calculation, the discrepancy between the measured and calculated S-parameters is considered as a loose constraint. The mean values of intrinsic elements are used to calculate the S-parameters.

$$\epsilon_2 = \frac{1}{N} W_{pq} \sum_{p=1}^2 \sum_{q=1}^2 \sum_{i=0}^{N-1} \left| \frac{\text{Re}(S_{ij}^s) - \text{Re}(S_{ij}^m) + j[\text{Im}(S_{ij}^s) - \text{Im}(S_{ij}^m)]}{S_{ij}^m} \right|^2 \quad (21)$$

where

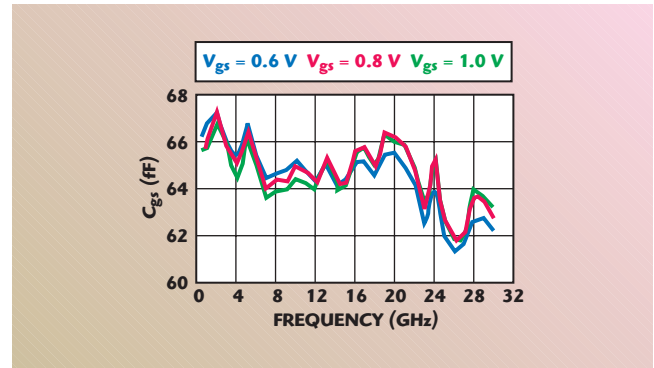
S^s = Modeled S-parameters

S^m = Measured S-parameters

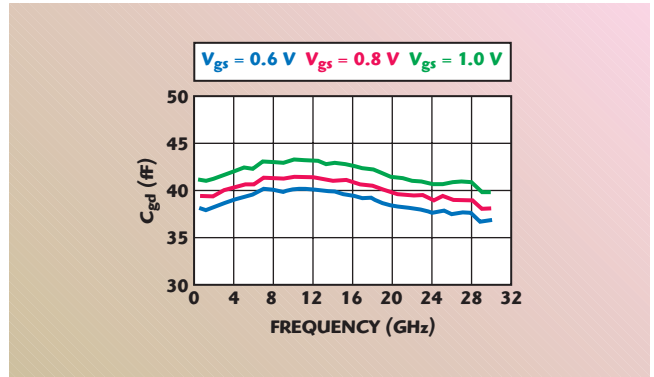
W_{pq} (Fixed at 0.25) = Weight Factors

The extended error vector is then composed as follows:

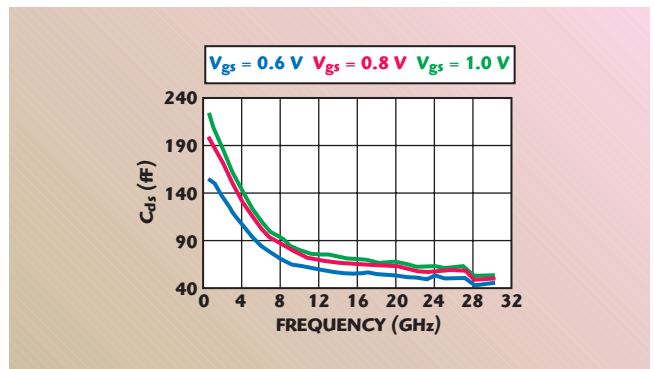
$$\epsilon = \begin{pmatrix} \epsilon_1 \\ \epsilon_2 \end{pmatrix} \quad (22)$$



▲ Fig. 3 C_{gs} frequency characteristics ($V_{ds} = 1.0$ V).



▲ Fig. 4 C_{gd} frequency characteristics ($V_{ds} = 1.0$ V).



▲ Fig. 5 C_{ds} frequency characteristics ($V_{ds} = 1.0$ V).



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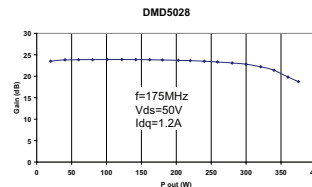
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DMD1012	100	50	13	500	28	PP
DMD1020	150	50	13	400	28	PP
DMD1028	300	60	16	175	28	PP
DMD1029	350	60	16	175	28	PP
DMD1037	140	50	13	175	28	SE
DMD5010	125	60	13	400	50	PP
DMD5012	100	65	15	500	50	PP
DMD5028	300	60	20	175	50	PP
DMD5029	350	60	20	175	50	PP

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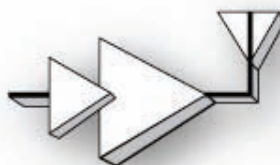
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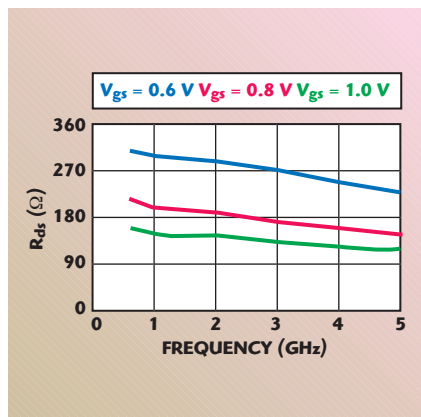
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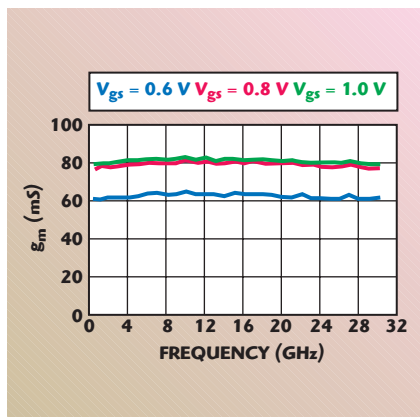
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▲ Fig. 6 R_{ds} frequency characteristics ($V_{ds} = 1.0$ V).

EXTRACTION PROCESS

A flowchart of the iterative process is shown in **Figure 2**. First, the initial extrinsic resistances and substrate elements are subtracted from the Z-parameters. The reduced Z-parameters are then converted to Y-parameters and the values of intrinsic elements are determined using Equations 14 to 19. Next, the extended error vector ϵ is

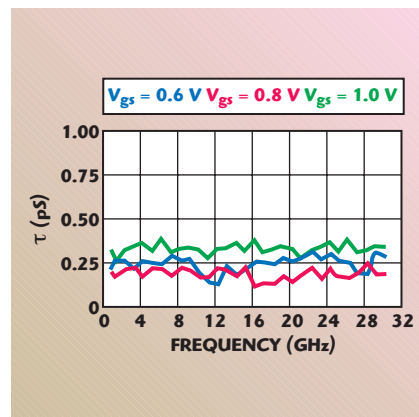


▲ Fig. 7 g_m frequency characteristics ($V_{ds} = 1.0$ V).

estimated from Equation 22. The values of R_g , R_d and R_s are updated to reduce ϵ using the Powell method.

EXPERIMENT

The MOSFET device has a channel mask length, $L = 0.13$ μm , a finger width, $W = 5$ μm , and a number of gate fingers, $N = 16$. Once the extrinsic elements are known, it is easy to determine the



▲ Fig. 8 τ frequency characteristics ($V_{ds} = 1.0$ V).

intrinsic elements for all biases. **Figures 3 to 8** show the intrinsic elements dependence on the gate and drain biases.

The results show that the extracted parameters remain almost constant with frequency. However, it also can be found that frequency dispersion effects exist in the extraction of R_{ds} and C_{ds} . This verifies that those components are frequency independent and the

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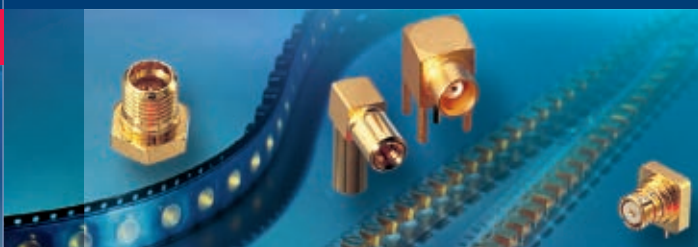
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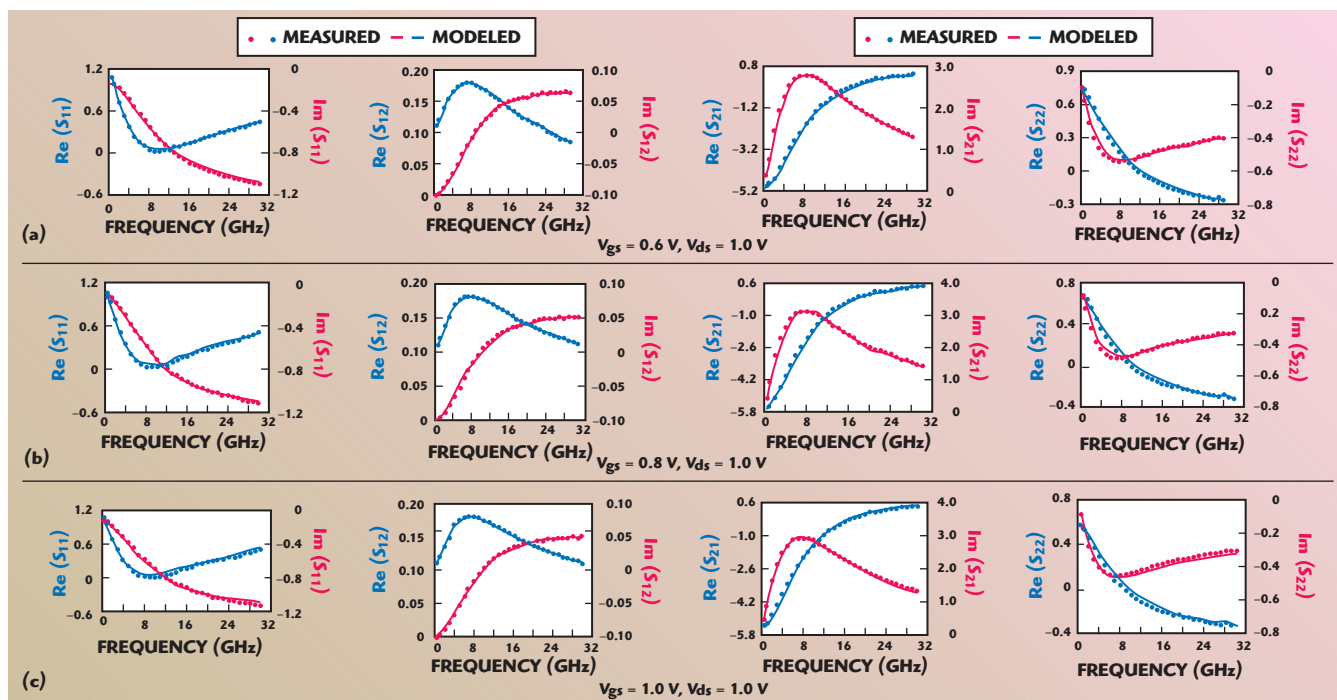
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▲ Fig. 9 Comparison of modeled and measured S-parameters for different biases.

method is accurate and reliable. **Figure 9** compares the measured and modeled S-parameters for the

MOSFET in the frequency range of 0.5 to 30 GHz under different bias conditions ($V_{ds} = 1.0$, $V_{gs} = 0.6$,

0.8, 1.0). The modeled S-parameters agree very well with the measured ones.



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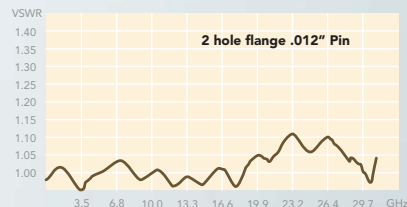
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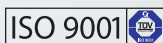


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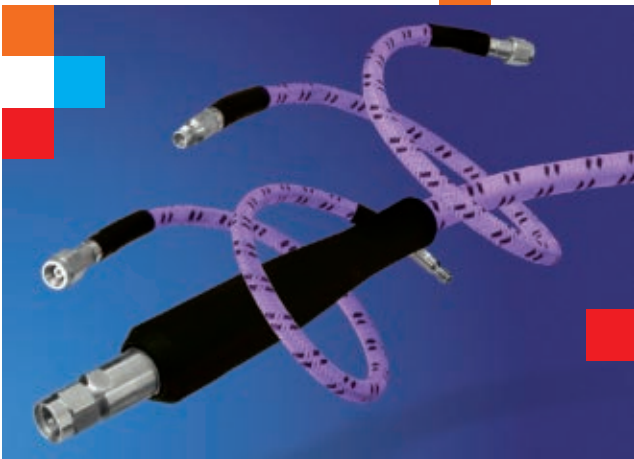
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CONCLUSION

An improved extraction technique for MOSFET small-signal model parameters is developed. The approach is based on a combination of analytical and optimization methods. ADS is then used to optimize only the parasitics with very small dispersion of initial values. Good agreement is obtained between the simulated and measured results over a wide range of bias points up to 30 GHz. ■

ACKNOWLEDGMENTS

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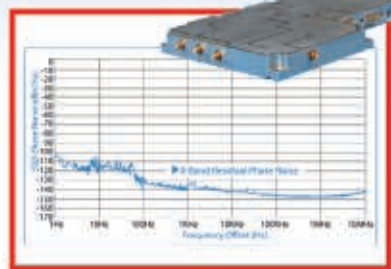
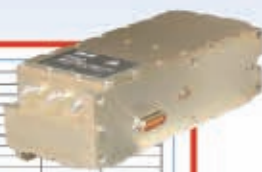
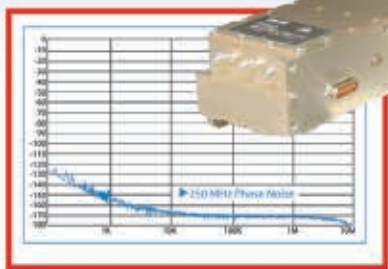
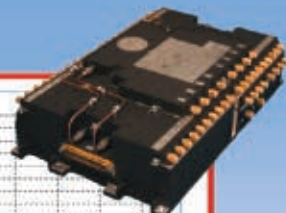
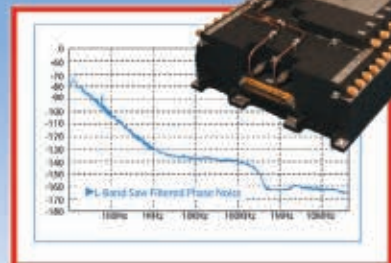
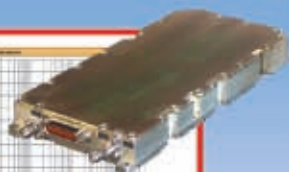
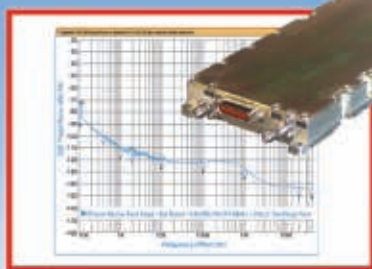
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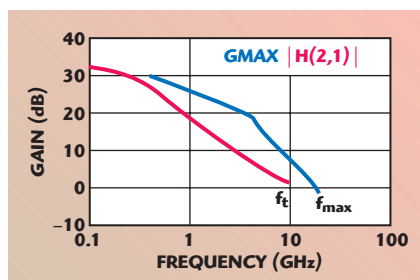
A 400 W pulsed output power GaN HEMT amplifier operating over the 2.9 to 3.5 GHz band (17 percent bandwidth) has been developed. Under pulsed RF drive, with 10 percent duty cycle and 100 μ s pulse width, the amplifier delivers an output power in the range of 401 to 446 W over the band, with a drain efficiency of 48 to 55 percent when biased at a drain voltage of 65 V. The amplifier uses AlGaIn/GaN HEMTs with a total device periphery of 44.4 mm and advanced source-connected field plates for high breakdown voltage. These wideband high power amplifiers are suitable for use in frequency agile pulsed applications such as military radar, air traffic control radar and communications jamming.

The high power and wide bandwidth potential of GaN HEMT devices is well known.¹ RFMD has been developing high power amplifiers using GaN HEMTs for various applications. A 250 W amplifier in the 2.14 to 2.5 GHz band for wireless infrastructure applications in the WCDMA and WiMAX bands was reported previously.² Such wide bandwidth is essential for the next-generation frequency agile software-defined radio (SDR) architectures that use reconfigurable radios to support multiple frequency bands and various standards.³

The military and commercial communities require high power and broadband modules for pulsed radar surveillance and air traffic control applications. The market is looking for the next-generation of devices that provide higher power and broader bandwidth and are able to support 1.2 to 1.4 GHz L-band for IFF, TACAN and TCAS pulsed applications and 2.7 to 3.5 GHz S-band pulsed applications.

These devices will enable suppliers to power combine fewer devices and reduce the size and weight power modules of greater than 1 kW for use in radar systems.

To obtain high power in existing power amplifier technologies, such as silicon laterally diffused metal oxide semiconductor (Si LD-MOS) and gallium arsenide pseudomorphic high electron mobility (GaAs PHEMT), large periphery devices are required. The resulting inherent large device parasitic capacitances per watt of output power lead to low device input and output impedances. Matching such low impedance to a 50 Ω system severely limits the bandwidth achievable. This also limits the maximum power obtainable in a package and further power combining is needed on the board. Wide band-gap material systems like gallium nitride (GaN) can be operated at high drain voltage and have low parasitic capaci-



▲ Fig. 1 GaN unit cell current and power gain performance.

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TABLE I

SUMMARY OF GaN PROCESS DC PARAMETERS

Parameter	Typical Value	Units
I_{dss}	800	mA/mm
I_{d-max}	900	mA/mm
Peak gm	225	mS/mm
V_p	-4.5	V
$V_{br}(GD)$	>150	V

tances per watt of output power. A combination of wider bandwidth and high output power can be achieved in a small package. This simplifies the design of kW transmitters for radar and jamming applications by reducing the number of devices required and minimizing losses in external combining networks.

THEORY

In theory, purely real impedances can be matched to a $50\ \Omega$ system over any bandwidth using an infinite number of matching elements. However, actual devices have optimum impedances with a reactive component. Complex loads can be matched only over a limited bandwidth as defined by Fano's limit.⁴ The maximum bandwidth ratio achieved using an infinite lossless matching network is given by

$$\frac{F_{high} - F_{low}}{F_o} = \frac{\Pi}{-Q_L \ln(\Gamma)} \quad (1)$$

where Q_L is the Q-factor of the device optimum source or load impedance to be matched and Γ is the minimum reflection coefficient needed across the band. This bandwidth is further limited in practice due to the

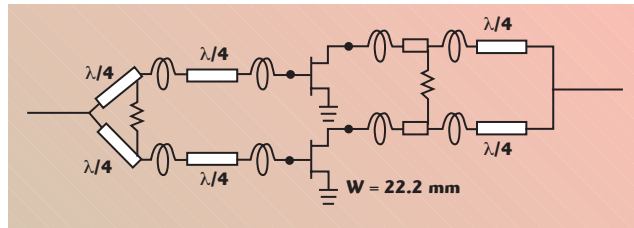


Fig. 2 Schematic of the amplifier circuit.

finite number of matching sections and the matching network losses. Hence, low Q-factors for the optimum source and load impedances are critical to obtaining a broad bandwidth. A suitable figure of merit, for high power broadband capability of a device technology, is a low pF/W gate and drain capacitance.

GaN HEMT TECHNOLOGY

RFMD's baseline AlGaIn/GaN HEMT technology is based on devices with a standard $0.5\ \mu\text{m}$ gate length and an advanced source connected field plate to obtain breakdown voltages in excess of 150 V. To be able to handle high-power densities in excess of 10 W/mm, a SiC substrate is used that provides excellent thermal conductivity and minimizes temperature dependent memory effects. The device topology and the baseline fabrication process are detailed in an earlier publication.⁵

Typical DC characteristics for the gallium nitride HEMT process are provided in Table 1. A typical device, biased at a drain voltage of 65 V, exhibits a peak current density of 0.9 A/mm. The current and power gain cut-off frequencies (f_t and f_{max}), as measured from small periphery devices, are 11 and 18 GHz respectively, as shown in Figure 1.

Under class AB bias and CW operation at 3.3 GHz, a typical 2.2 mm unit cell device obtains 56 percent peak power added efficiency (PAE) and a peak output power of 21.9 W. This corresponds to a power density of 9.9 W/mm. This is about three times the 3.2 W/mm power density obtained at 28 V drain bias from a device without the field plate. The series equivalent optimum source and load impedances are $Z_s = 3.8 + j10.5\ \Omega$ and $Z_L = 30 + j47\ \Omega$, respectively. These indicate low gate and drain capacitances of approximately 0.46 pF/W and 0.07 pF/W, respectively, which is about one fifth of that of equivalent silicon devices. Using this series equivalent source impedance, the theoretical maximum bandwidth ratio for a 15 dB return loss can be calculated to be 57 percent. These low capacitances contribute to the higher bandwidth obtained, compared to other device technologies.

CIRCUIT DESIGN

The amplifier circuit, seen in Figure 2, uses two 22.2 mm periphery devices, combined using a Wilkinson power divider/combiner⁶ on the input and output, respectively. This topology achieves a wider bandwidth than would be obtained using a single 44.4 mm device. Along with the power division/combination function, the Wilkinson combiners also perform the impedance transformations required to provide the optimum source and load impedance to the devices.

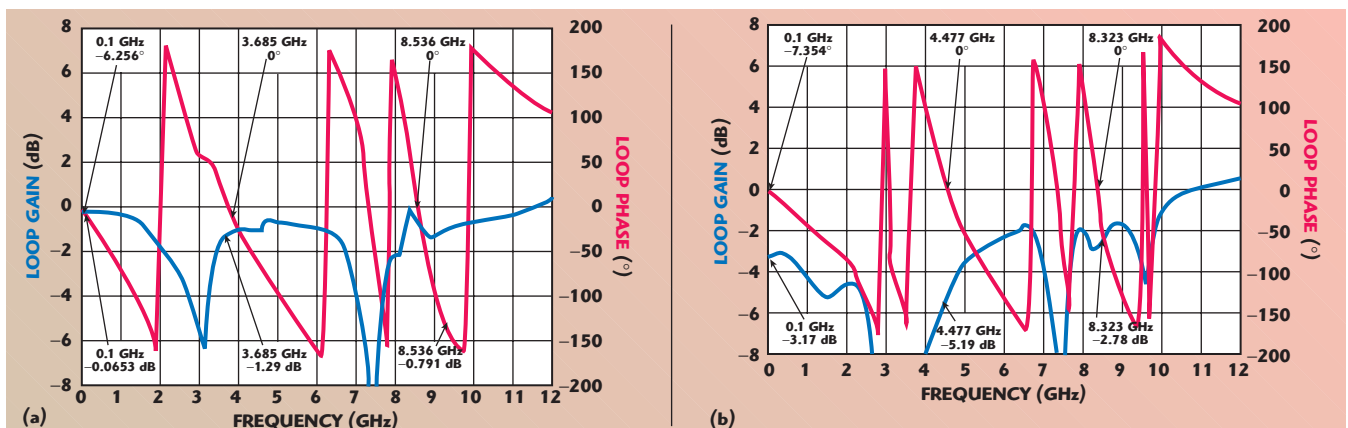


Fig. 3 Loop gain and phase analysis (a) without isolation resistor and (b) with isolation resistor.

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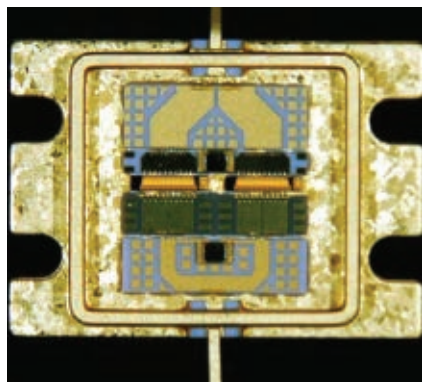
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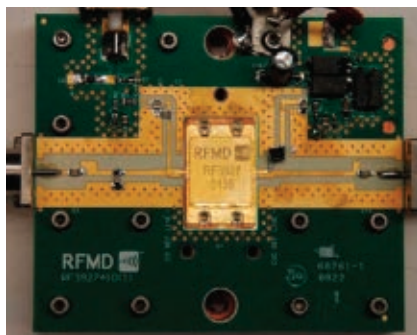
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▲ Fig. 4 Photograph of the 400 W GaN HEMT amplifier.

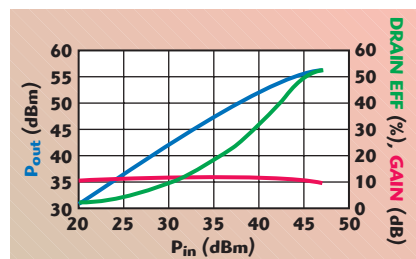
The unit cell source and load pull impedance measurements were used to estimate the large periphery device's source and load optimum impedances. Due to the higher gate capacitance, a two-stage impedance transformation was used at the gate to obtain a broader bandwidth. The drain section consists of an inductive element to provide the reactance needed for the optimum load and a single stage Wilkinson combiner/transformer. Electromagnetic field models were used extensively to



▲ Fig. 5 Photograph of the 400 W 50 Ω test fixture.

model the frequency performance of the combiner transformer elements.

Additionally, extensive stability analysis and odd-mode oscillation loop analysis were conducted. This type of combining network is prone to the formation of out of frequency band oscillation loops. Therefore, the design needs significant analysis over a wide frequency range to determine if any potential odd-mode oscillation loops exist. A previous work⁷ provides a detailed description of applying stability analysis to multi-device amplifiers, using linear analysis and S-para-



▲ Fig. 6 RF output power at the mid-point of the pulse, drain efficiency and gain measured at 3.4 GHz.

meters. Applying this methodology to gallium-nitride-based amplifiers, an extensive analysis of odd-mode oscillation loops is provided by Yanamaka, et al.⁸ For an odd-mode loop to cause stability issues, the following conditions must be met

$$\text{Loop phase angle } (\Gamma) = 0^\circ \quad (2)$$

$$\text{Loop gain magnitude } (\Gamma) > 1 \text{ (0 dB)} \quad (3)$$

Generally, however, to provide adequate design margin, loop gain less than -2 dB should be maintained across a frequency band where G_{\max} is greater than 0 dB.

A similar methodology was applied to this amplifier design; an example of the loop analysis is shown in **Figure 3**. The amplifier's loop gain and phase, using Wilkinson combiner networks not using an isolation resistor between the ports, is shown. It can be seen that the loop phase angle meets the criteria for oscillation at two distinct frequencies 3.685 and 8.536 GHz. Additionally, the loop phase is close to the criterion at low frequency. In all three cases the loop gain requirement is not met. However, the loop gain margin is less than the adequate limit defined. The figure also shows how the loop stability can be

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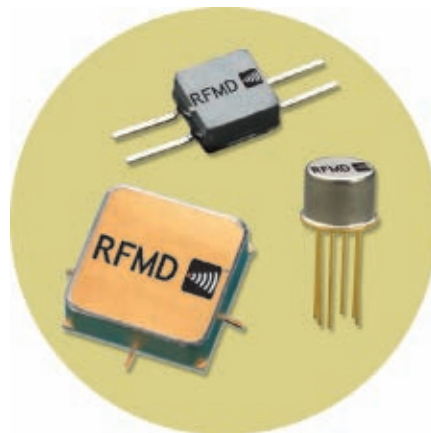
TABLE II

SUMMARY OF THE AMPLIFIER RF PERFORMANCE

Frequency (GHz)	Pk Pout (W)	Drain Eff (%)	PAE (%)
2.9	446.4	55.5	49.1
3.0	432.9	55.1	49.0
3.1	414.8	50.8	44.6
3.2	419.3	54.0	47.3
3.3	405.4	48.4	42.4
3.4	434.1	52.6	46.5
3.5	401.5	53.8	47.9

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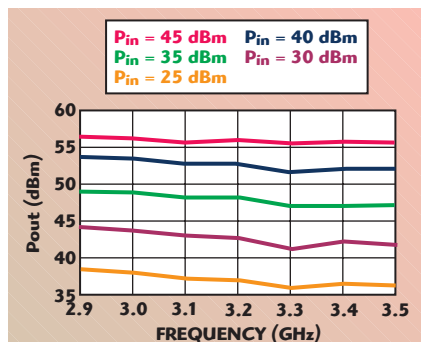
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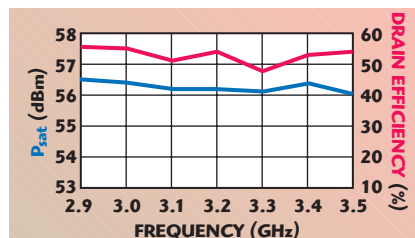
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▲ Fig. 7 RF output power at the mid-point of the pulse over the 2.9 to 3.5 GHz band.

increased by adding an isolation resistor to the Wilkinson combiner and by optimizing the gallium nitride device layout. The loop gain has been reduced to levels meeting the design margin requirements at all three frequency points.

The devices are packaged in a 15 x 17 mm package (see **Figure 4**).⁹ The combiner/dividers were implemented on high dielectric constant substrates to achieve the small dimensions required to fit inside the package. The quarter-wave transformations were designed to obtain a 35 Ω impedance

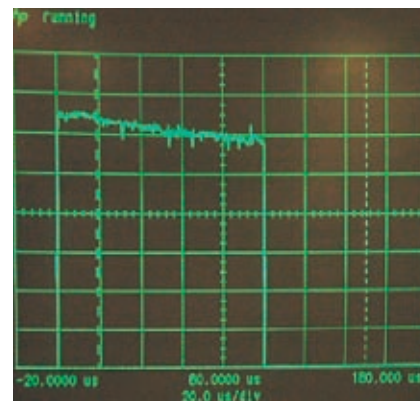


▲ Fig. 8 Measured saturated output power and drain efficiency over the 2.9 to 3.5 GHz frequency band.

at the package leads. The evaluation board used for testing further transforms the impedance to 50 Ω and is shown in **Figure 5**.

PULSE POWER PERFORMANCE

The RF performance of the device was evaluated after optimizing the on-board matching. The amplifier was biased in class AB mode at a fixed drain voltage of 65 V and a drain current of 440 mA. The RF input was pulsed using a 100 μ s wide pulse with a 1 ms period and the output power was measured at the center of the pulse. The drain current pulse waveform was monitored to cal-



▲ Fig. 9 Measured power droop of 0.25 dB over a 100 μ s pulse at 56.4 dBm output power (at the center of the pulse) with 10% duty cycle.

culate the drain efficiency. The amplifier was tested over the frequency range of 2.9 to 3.5 GHz.

Figure 6 shows the measured output power at the mid-point of the pulse, the drain efficiency and the gain at 3.4 GHz as a function of the input power. A peak output power of 434 W was obtained at 3.4 GHz with a drain efficiency of 52.6 percent. **Figure 7** shows the measured output power over frequency for a range of input power. The broadband power capability of the device is apparent from the plot.

Figure 8 shows the peak saturated output power and drain efficiency over the frequency band, while **Table 2** summarizes the data. An output power in excess of 401.5 W was obtained over the entire band, with better than 48.4 percent drain efficiency.

The pulse droop performance at 56.4 dBm output power (see **Figure 9**) shows approximately a 0.25 dB droop over the complete 100 μ s pulse, and less than 0.15 dB across the middle 50 percent of the pulse. This confirms the excellent thermal capability of the GaN on SiC dies in the package, even under the high power density at which they are operating.

CONCLUSION

A compact, greater than 400 W, wideband, AlGaIn/GaN HEMT power amplifier has been demonstrated, operating at 65 V with better than 48.4 percent drain efficiency over a 600 MHz bandwidth from 2.9 to 3.5 GHz, under pulsed condition with a 10 percent duty cycle and 100 μ s pulse width.

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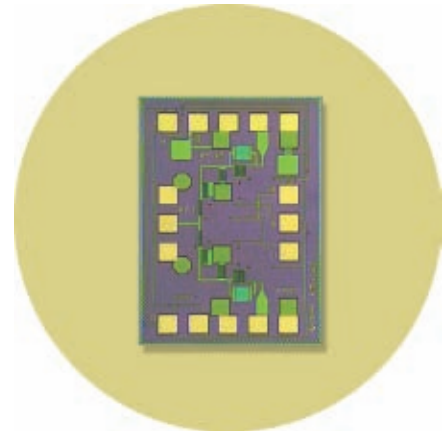
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	Min	Typ	Max	Units	Min	Typ	Max	Units	Min	Typ	Max	Units
FMS2023	-0.9	-0.7	-	dB	-	-50	-43	dB	25	27	-	dBm
FMS2024	-1.6	-1.1	-	dB	-	-37	-34	dB	22	24	-	dBm
FMS2027	-1.5	-1.3	-	dB	-	-42	-40	dB	21	22.5	-	dBm
FMS2029	-1.65	-1.4	-	dB	-	-60	-45	dB	23.5	25.2	-	dBm

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The combination of GaN HEMT device technology and the impedance matching topology achieves high power and broad bandwidth in a small package. The design incorporates Wilkinson combiner/transformers that provide excellent low loss, wide bandwidth performance in a compact design. The loop stability is a critical design consideration that was addressed to ensure stability over all frequencies.

These amplifiers are well suited for pulsed applications, including advanced radar systems. The small size and high power obtained in a single package greatly simplifies the design of kW transmitters by reducing the number of devices needed in parallel. In addition, improvement to overall system bandwidth and efficiency is achieved as the combiner losses are further reduced. Additional savings in inventory and critical real estate needs are further advantages of using this device. ■

ACKNOWLEDGMENT

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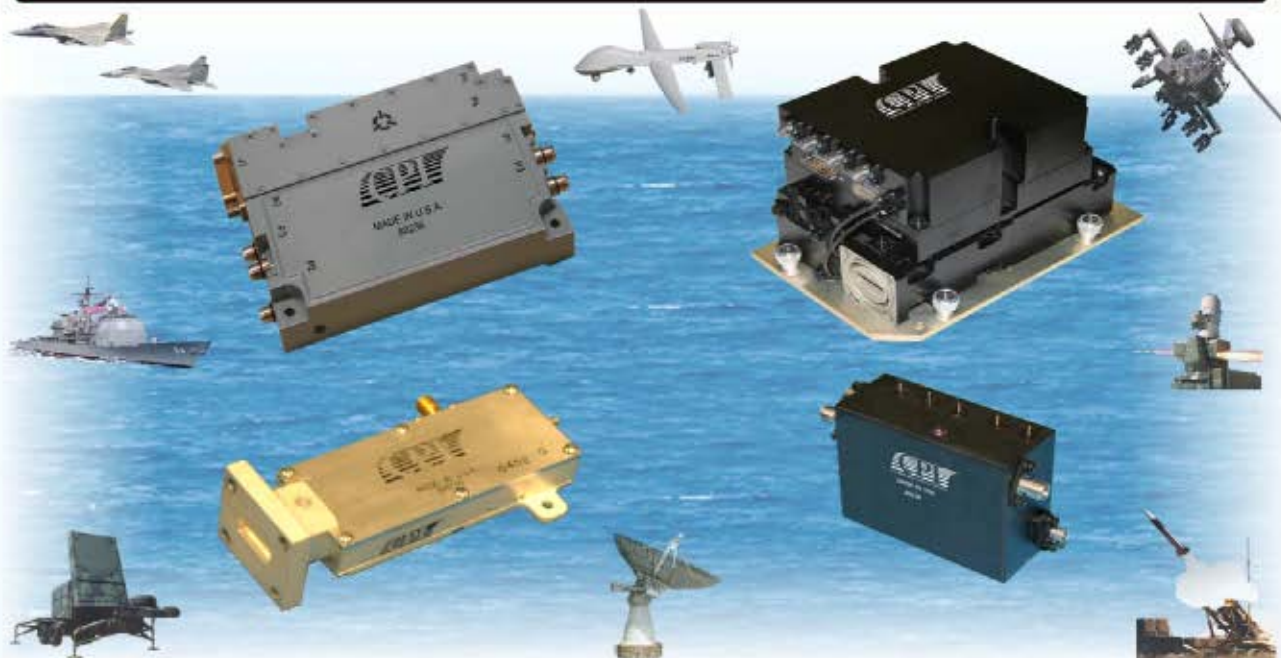
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LOW FREQUENCY 3-D ELECTROMAGNETIC ANALYSIS OF ANECHOIC CHAMBER PERFORMANCE

The advantages of anechoic chambers utilized for antenna measurements, as compared with conventional outdoor antenna test ranges, such as security, interference-free radiation and immunity to weather, are well known. Typical anechoic chambers comprise a shielded enclosure with the internal metallic surfaces covered by absorbing materials, a source antenna to illuminate the device under test (DUT), and positioning equipment on which the DUT is installed and rotated to acquire antenna pattern data. The dimensions of the shielded enclosure are primarily determined by the lowest operating frequency, and thus the required size will be significantly increased if the chamber operation is required down to VHF and/or UHF frequency bands. This in turn increases the construction and absorbing material costs. As a result, the advantage of an indoor chamber is often questioned when considering the VHF or UHF band as the lowest operating test frequency range. The main concern in this case is the projected amount of real estate required for construction of the chamber. A trade-off exists between the desire to lower the cost by reducing chamber size and the desire to ensure minimum performance levels by increasing the chamber size.

In order to achieve a minimum level of accuracy in the antenna measurement, a corresponding minimum level of DUT test zone illumination quality and overall chamber reflectivity needs to be achieved. This requires that turn-key chamber suppliers need to be able to accurately analyze the chamber performance. The ability to accurately characterize chamber performance results in an optimum design implemented at minimum cost.

To date, the method most often implemented in the industry to analyze anechoic chambers has been based on ray tracing. This method suffers from poor accuracy in cases where the room dimensions are only a few wavelengths at the lowest operating frequency. Several factors contribute to poor accuracy for these cases:

- The specular region, where reflections significantly impact the quality of the DUT test zone, has characteristic dimensions that encompass a few wavelengths of the wall surface covered by the absorbing materials, which at VHF and UHF frequencies may exceed side wall, floor and ceiling characteristic dimensions.

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- As the effective specular area is large, it is difficult to define the correct incidence angle of the specular illumination for the ray tracing analysis.

- It is difficult to accurately predict or measure the reflection coefficient of the wall absorber at off-normal incidence at low frequencies.

- The phase of the reflection coefficient of the absorber material is difficult to accurately measure. Hence, only RMS or RSS fields can be calculated in the DUT test zone, thus delivering only approximate analysis results.

- In some cases assumptions are made for the reflectivity at off-normal incidence angles at VHF and UHF bands, based on similarity to reflectivity degradation curves at off-normal incidence at higher frequencies (> 2 GHz).¹ However, this extrapolation has proven to be inaccurate at a number of installed anechoic chambers.

A useful improvement to the ray tracing method is the aperture integration method, in which the fields reflected from side walls into the test zone are calculated using Kirchhoff integration over apertures (portions of the side walls, floor or ceiling), and the field in the test zone is obtained as a sum of these reflected fields together with the direct radiation of the source antenna.

Although this method is better suited for analysis of anechoic chambers, the available accuracy is still limited and is determined by the information available on the reflectivity (magnitude and phase for two orthogonal polarizations) of the absorbing materials used in the chamber at both normal and off-normal incidence, which is (as indicated earlier) too problematic at the VHF and UHF bands. In addition, neither the aperture integration nor ray tracing methods take into account multiple reflections within the chamber, which is typically a significant effect at these frequencies.

IMPACT OF INACCURATE CHAMBER ANALYSIS

Lack of accuracy in chamber performance prediction may lead to non-optimum chamber design. However, less than optimum performance is not always easy to identify. For example, field probing of the test zone may not show the full extent of field

variations and ripples originating from reflections within the chamber interior due to the long period of the interference pattern produced by the reflections and direct radiation at low frequencies.

In order to ensure adequate chamber performance, field probing should be performed over as broad a frequency range as possible. Smooth changes of the field in the test zone over a broad frequency range are a positive sign, indicating that the chamber performs well. Small variations of the recorded signal over a broad frequency range for multiple matched transmit/receive polarizations is another positive sign of excellent chamber performance.

3-D ELECTROMAGNETIC SIMULATION

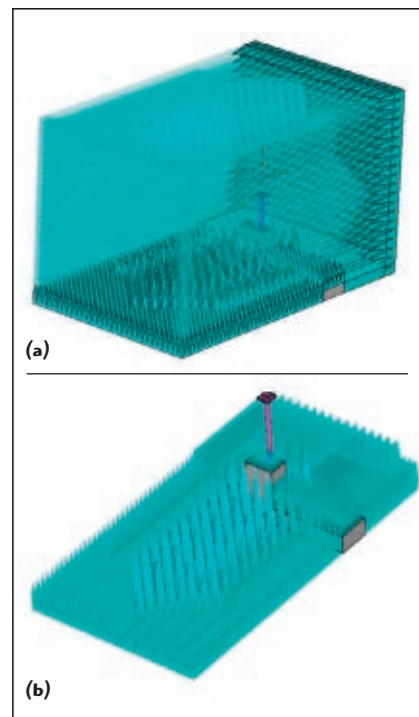
Given the limitations stated above for the aforementioned analysis techniques at low frequencies, it is obvious that a more rigorous and comprehensive analysis is required. An appropriate analysis is a 3-D electromagnetic simulation as described below.

A short time ago, no standard software package could be utilized to solve the problem of analyzing an anechoic chamber for comprehensive 3-D field quality. Recently, thanks to significant steps made in PC technology and advances in 3-D electromagnetic computer simulation packages utilizing time-domain techniques,² such analysis is now possible.

ORBIT/FR has implemented a full 3-D simulation for anechoic chambers at low frequencies using a commercial transient solver package available from CST. Typical simulation results are presented below to illustrate the effectiveness of the 3-D time domain technique as applied to the analysis of anechoic chambers at low frequencies.

The primary analyses performed for the chamber include field uniformity over a volume of interest within the chamber, such as the DUT test zone, including subsequent determination of amplitude taper and ripple; phase variation; and induced cross-polarization levels in the chamber fields. These metrics are a function of the following parameters:

- Absorbing material layout and grades



▲ Fig. 1 Isometric view of the anechoic chamber design (a) and absorber layout on the floor (b).

- Source antenna/DUT separation
- Operating frequency
- Source antenna beamwidth
- DUT positioning equipment
- DUT supporting structure geometry and materials

The analysis can provide information leading to the proper selection of source antenna, source antenna/DUT separation, absorber layout and minimum chamber size required to achieve desired performance levels.

CHAMBER MODELING METHODOLOGY

The most efficient way to model the anechoic chamber is to create a database of standard components, including absorbing materials of different types such as pyramids, wedges, hybrids (a combination of pyramids backed by ferrite tiles), walkways, etc. Each type of material may contain different size models. For example, pyramids may be produced with various heights ranging from 2 to 96 inches or more. For UHF and VHF applications the larger heights are utilized, typically from 36 to 96 inches.

Material loading levels are input and stored in the database. These are based on measurements of the material properties $\epsilon'(f)$, $\epsilon''(f)$, $\mu'(f)$, $\mu''(f)$

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BD0826J50200A00	0.8-2.6	1.3	26
B0922J7575A00	0.9-2.2	1.2	26
B0922J7575A50	0.9-2.2	1.1	25
BD1222J50200A00	1.2-2.2	0.6	30
BD1631J50100A00	1.6-3.1	1	33
BD1722J50100A00	1.7-2.2	1	26
BD1722J50150A00	1.7-2.2	0.7	30
BD1722J50200A00	1.7-2.2	0.7	30
BD2130J5050A00	2.1-3.0	1.2	37
BD2425J5050A00	2.4-2.5	0.9	37
BD2425J50100A00	2.4-2.5	0.75	42
BD2425J50200A00	2.4-2.5	0.8	37
BD2326L50150A00	2.3-2.6	1.1	29
BD2326L50200A00	2.3-2.6	1.1	29

Part Number	Frequency (Ghz)	Insertion Loss (dB)	Common Mode Rejection Ratio (dB, typical)
BD3150L50100A00	3.1-5.0	1.1	28
BD3150L50200A00	3.1-5.0	1.2	25
BD4859L5075A00	4.8-5.9	1.3	31
BD4859L50100A00	4.8-5.9	1.1	30
BD4859L50150A00	4.8-5.9	1	28
BD4859L50200A00	4.8-5.9	1.4	26
B4859A53	4.8-5.9	0.9	27
BD2425N5075A00	2.4-2.5	0.9	35
BD2425N50100A00	2.4-2.5	0.7	37
BD2425N50200A00	2.4-2.5	0.7	29
BD3150N50100A00	3.1-5.0	0.7	26
BD4859N5050A00	4.8-5.9	0.7	27
BD4859N5075A00	4.8-5.9	0.5	28
BD4859N50100A00	4.8-5.9	0.6	26
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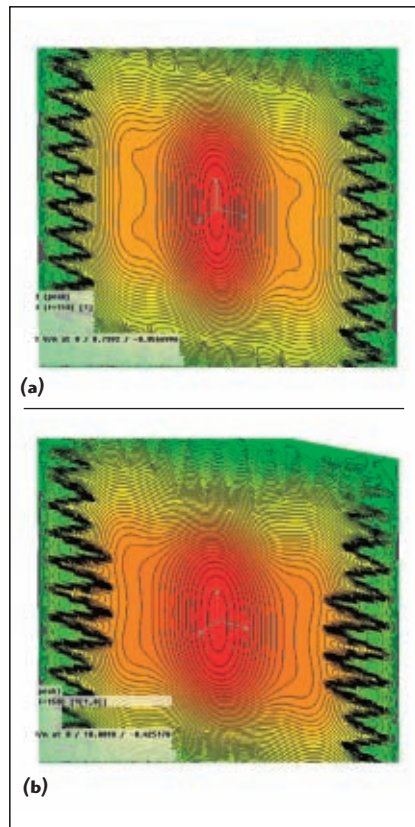
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over the desired frequency range. Accurate characterization of the material using these parameters is critical for an acceptable simulation.

Typically, the absorber layout contains different types and different grades of absorbing materials, as shown in **Figure 1**. The design shown is for an anechoic chamber size of $H = 6$ m, $W = 6$ m, $L = 10$ m, intended to operate down to 150 MHz. The floor contains a "diamond patch" of diagonally oriented pyramidal pieces of absorbing material located in the "specular" region of the floor, and is surrounded by lower grades of pyramids and wedge absorbing materials at the far end of the floor. The positioning system, a fiberglass tower supporting the DUT and walkway are also shown in the layout, and are accounted for in the simulations.

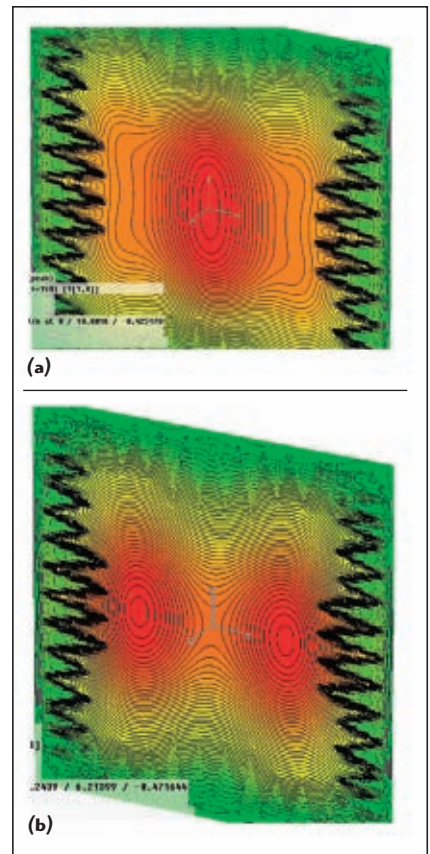
OPTIMAL SELECTION OF ABSORBER LAYOUT AND GRADES

Here, the effect of the absorber layout and absorber grades on the test zone performance is discussed. It is assumed that the basic chamber layout is similar to the one shown. A study and comparison of the test zone performance are made for two cases in which the receive wall and the "diamond patch" are made of 36 and 48 inches high pyramidal absorbers, respectively. The test zone fields for the two cases are presented in **Figure 2** in the form of con-



▲ Fig. 2 Test zone field contour at center of the test zone (a) 36-inch pyramidal absorber; (b) 48-inch pyramidal absorber.

tour plots of the fields in the central cross-section of the test zone. It is evident upon inspection that the field in case b) is more uniform than in case a), indicating that the performance is superior using the 48 inch pyramids.



▲ Fig. 3 Test zone field contour as a function of source antenna/DUT separation: (a) 3 m separation; (b) 6 m separation.

It is also readily observed that the reflectivity of the side walls (H-plane of the incident field) is inferior to that of the floor and ceiling (E-plane of the incident field), yielding the "ellipse" like field distribution in the test zone.

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EFFECT OF SOURCE ANTENNA/DUT SEPARATION ON TEST ZONE PERFORMANCE

The separation between the source antenna and the DUT is an important parameter at VHF and UHF frequency bands and can strongly influence the test zone performance. It is well known that at microwave frequencies (> 2 GHz) the absorbing materials perform reasonably well for large incident wave angles such as 65° . However, at VHF and UHF frequencies, the absorber performance at large off-normal angles is sharply reduced. The examples shown in **Figure 3** illustrate field contour plots calculated for the following:

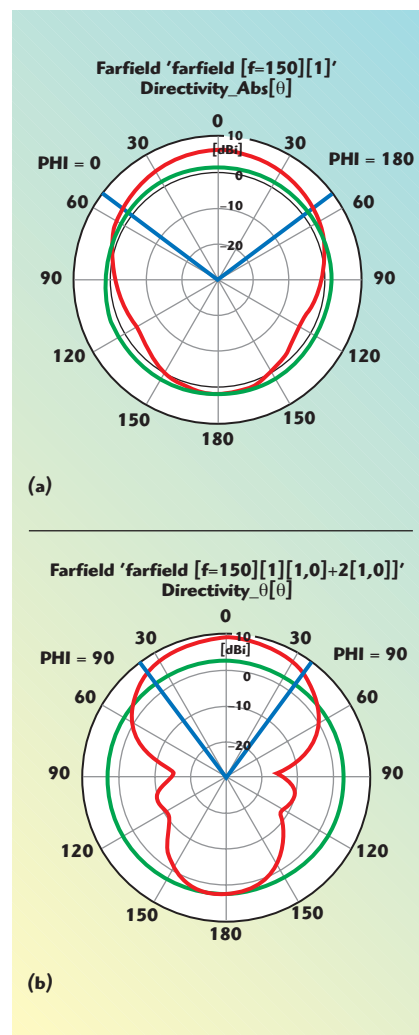
- A 3 m source antenna/DUT separation, where the incident wave angle to the side walls, floor and ceiling is approximately 27° .
- A 6 m source antenna/DUT separation, where the incident wave angle to the side walls, floor and ceiling is approximately 45° .

As is readily observed, the longer separation leads to an unexpected and undesired field distribution across the test zone. The field structure results in a local minimum in the center of the test zone, which represents an unstable condition that tends to change rapidly with frequency, and, therefore, results in poorly controlled field uniformity in the test zone.

EFFECT OF SOURCE ANTENNA BEAMWIDTH (BW) ON TEST ZONE PERFORMANCE

Another important parameter in the design of the anechoic chamber is the beamwidth of the source antenna. As mentioned previously, the reflectivity in the H-plane of the chamber is typically worse than in the E-plane. Poor reflectivity can be improved to some degree by reducing the beamwidth of the source antenna. However, too large of a beamwidth reduction leads to increased amplitude taper and reduction in the size of the test zone. Moreover, beamwidth reduction is not easy to achieve at VHF and UHF frequencies, since this requires increased dimensions of the source antenna, which is not always practical in an anechoic chamber. Electromagnetic simulation is thus an important tool in analyzing the optimum choice of source antenna prior to anechoic chamber construction.

The simulation examples represent the test zone field contour plots obtained with a source antenna composed of a single log-periodic dipole (LPD) antenna as well as with a pair of LPD antennas separated by a half wavelength. The difference in H-plane patterns of the two source antennas is shown in **Figure 4**. Inspection of the contour plot lines in **Figure 5** reveals that the dual LPD array produces a more uniform field, exhibiting fields with nearly circularly symmetric contour lines.



▲ Fig. 4 H-plane patterns of LPD-based source antenna (a) single LPD antenna, 3 dB BW, $\approx 106^\circ$ and (b) pair of LPD antennas, 3 dB BW, $\approx 73^\circ$.

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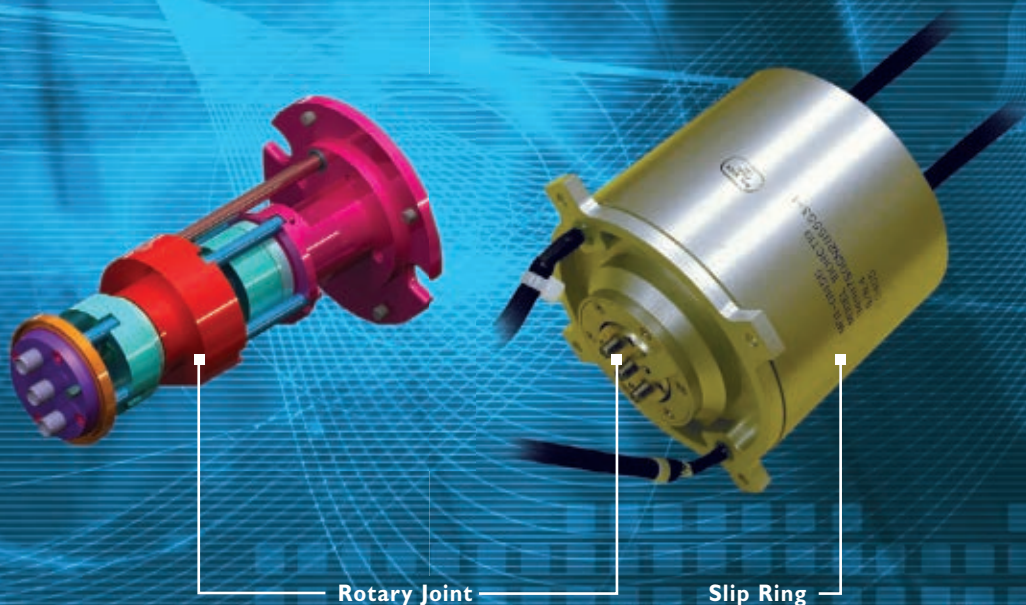
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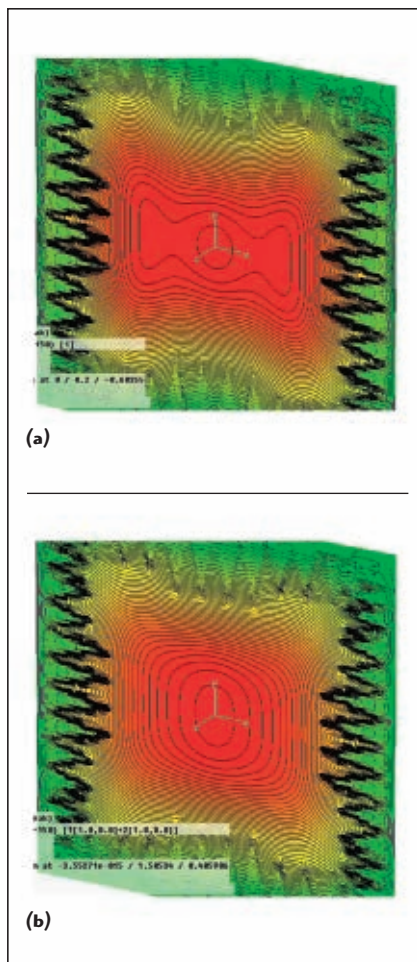
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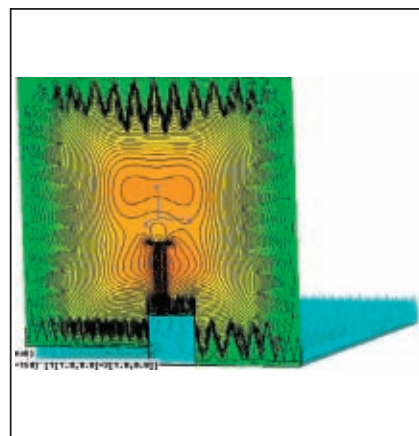
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▲ Fig. 5 Contour plots of test zone fields obtained using different source antennas: (a) single LPD antenna, 3 dB BW $\approx 106^\circ$; (b) pair of LPD antennas, 3 dB BW $\approx 73^\circ$.

EFFECT OF POSITIONING EQUIPMENT ON TEST ZONE PERFORMANCE

Positioning equipment and a walkway absorber path for operator access to the DUT are required elements in any anechoic chamber. As a result of their close proximity to the test zone, both may cause undesired and uncontrolled test zone field perturbations, especially at low frequencies. The effects of these elements on test zone performance are often hard or impossible to estimate prior to their installation. Electromagnetic 3-D computer simulation is a tool capable of taking these elements into account and to estimate the overall test zone performance in advance, prior to the chamber construction. **Figure 6** shows how the positioner and fiberglass tower that supports the DUT may affect the test zone



▲ Fig. 6 Fields in the test zone with positioner, walkways and fiberglass tower included.

field distribution. As is evident, the field may lose important symmetry properties and the peak of the field (or the center of the test zone) moves higher, sometimes above the DUT mounting location. Addition of absorbers on the positioner assembly can often reduce this effect.

CONCLUSION

Electromagnetic 3-D analysis of anechoic chambers at low frequencies such as the VHF and UHF bands, executed with the aid of time domain software, delivers significant advantages over previously utilized analysis methods, resulting in a much more accurate characterization of test zone fields, thus allowing a more cost-effective and higher performance chamber design.

The performance factors that may be evaluated include:

- Broadband analysis of the effects produced by absorber material layout and various absorber grades on test zone performance
- Definition of the optimal source antenna/DUT separation as a function of frequency
- Optimal choice of the source antenna(s)
- Analysis of the effects produced by DUT positioning equipment and mounts, as well as walkway absorber, on test zone performance. ■

References

1. L.H. Hemming, *Electromagnetic Anechoic Chambers: A Fundamental Design and Specification Guide*, Wiley-Interscience, Hoboken, NJ, 2002.
2. CST Studio Suite 2008.

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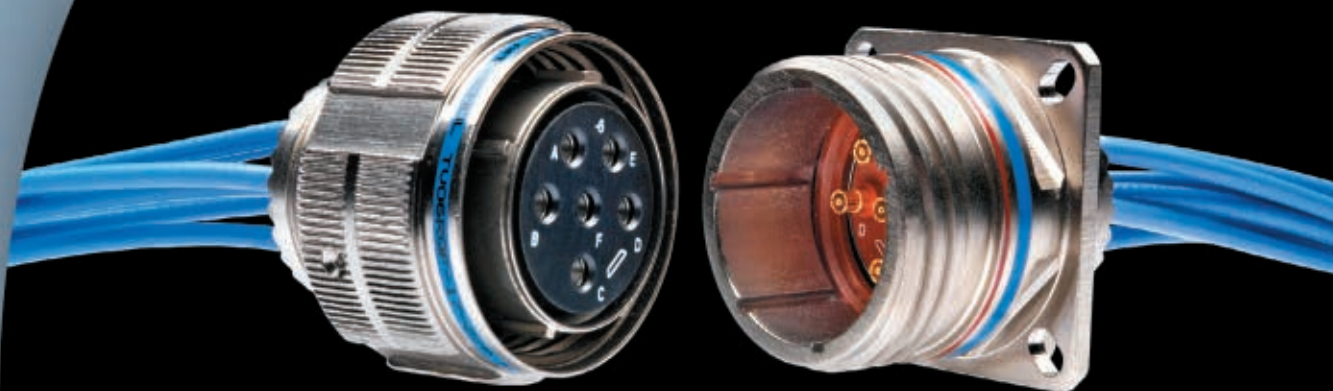
A COMPACT CPW-FED RECTANGLE-TRAPEZOID-RECTANGLE SHAPED MONOPOLE ANTENNA FOR ULTRA-WIDEBAND SYSTEMS

A novel CPW-fed rectangle-trapezoid-rectangle shaped monopole antenna composed of a trapezoid and two rectangles is presented. In this context, the flat monopole structure improves the impedance bandwidth and reduces the size of the antenna dramatically. The ultra-wideband (UWB) antenna design plays a role as a filter. The coplanar waveguide grounds are beveled and the impedance transformer patch (ITP) performs a 50 to 100 Ω impedance transformation. The impedance and radiation characteristics of this antenna are studied. The measured bandwidth, defined by a 10 dB return loss, is from 2.78 to 10.71 GHz. The overall size of the printed antenna is $31.45 \times 31.45 \times 0.8$ mm, which is very compact, low profile and can be integrated within an ultra-wideband transceiver. The proposed antenna also has the advantages of a very simple geometric structure, good radiation characteristics, almost omnidirectional radiation patterns and smooth gain characteristics. Therefore, it is a good candidate for ultra-wideband applications.

Ultra-wideband technology has been widely used in various wireless communications and has attracted much attention recently for communication systems. UWB is suitable for high-speed wireless communications within Wireless Personal Area Network (WPAN), because of its short-range, high data-rates, low-cost and low-power technology, utilizing the unlicensed radio spectrum from 3.1 to 10.6 GHz. The design of a UWB antenna is one of the most exciting tasks in these systems. Some coplanar waveguide (CPW) antennas have been proposed for wideband applications.¹⁻¹¹

One of the critical issues in UWB system design is the size of the antenna for portable devices, because the size affects the wide impedance bandwidth, gain and omni-directional radiation pattern. Therefore, to miniaturize an

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antenna capable of providing a broad impedance matching bandwidth and an acceptable gain is a challenging task.⁴ To increase the bandwidth, such techniques as constructing a simple bevel,⁵ using a smooth rounded element⁶ or using a shorting pin⁷ have been reported. In addition, CPW-fed monopoles¹⁻⁴ have also been introduced for their compact size, simple structure and ease of integration with microwave circuits.

In this article, a small size antenna is proposed using a CPW feed-line for UWB systems. Compared to the printed folded flared monopole antenna⁸ and the improved U-shaped stub rectangular slot antenna with a tuning pad for UWB applications,⁹ the proposed antenna can produce better gain and good radiation performance. This novel CPW-feed rectangle-trapezoid-rectangle shaped monopole antenna is composed of a trapezoid and a tangential rectangle. This monopole structure reduces the size, improves the impedance bandwidth and offers a smooth gain and almost omni-directional patterns. The detailed design and experimental results are pre-

sented and discussed in the following sections.

ANTENNA DESIGN

The proposed antenna has a simple structure, with one layer of dielectric and metal. The antenna is fabricated on a low-cost FR-4 substrate with a dielectric constant $\epsilon_r = 4.4$ and thickness $h = 0.8$ mm. The following design method has been used to develop the proposed CPW-feed antenna knowing the lowest frequency of the UWB operation ($f_L = 3.1$ GHz) and the effective dielectric constant of the transmission line (ϵ_{reff}). Excluding the feeder, the width (W_1) and length (L_1) of the antenna structure can be calculated using Equations 1 and 2

$$\epsilon_{\text{reff}} = \frac{\epsilon_r + 1}{2} \quad (1)$$

$$W_1 = L_1 = \frac{c}{2f_L \sqrt{\epsilon_{\text{reff}}}} \quad (2)$$

where

c = speed of light in free space

The rectangle-trapezoid-rectangle shape is printed on a substrate $L_1 = 31.45$ mm (0.3249λ) by $W_1 = 31.45$ mm (0.329λ) substrate, where λ is the free space wavelength at the 3.1 GHz frequency. The monopole antenna is fed by a 50 Ω CPW line with width $W_5 = 1.5$ mm and a spacing gap $G_1 = 0.18$ mm between the center conductor and the ground plane. The geometry of the proposed antenna is shown in **Figure 1**. The bevels in the ground plane enhance the operating

bandwidth. The flare angle is $\theta = 45^\circ$.

In this article, the impedance transformer patch (ITP) is designed to obtain a well-matched wideband antenna. Recognizing that the center frequency for UWB operation is $f_r = 7.85$ GHz and the dielectric constant is ϵ_r , the major ITP length (W_6) and the width (L_6) are chosen according to the following equations:

$$W_6 = \frac{c}{8f_r} \left(\frac{\epsilon_{\text{reff}} + 1}{2} \right)^{\frac{1}{2}} \quad (3)$$

$$L_6 = \frac{1}{W_6} = \frac{1}{\frac{c}{8f_r} \left(\frac{\epsilon_{\text{reff}} + 1}{2} \right)^{\frac{1}{2}}} \quad (4)$$

The ITP is formed by setting $W_6 = 4$ mm. When the length of the W_6 section increases, the ITP becomes a rectangle and the bandwidth increases gradually. The length of W_6 controls the effective area of the rectangle and is the primary parameter to determine the coupling between the antenna element and the ground plane.

The rectangle-trapezoid-rectangle shaped patch is the radiator of the proposed design. The parameter $L_T = (L_2 + L_5 + L_6 + L_7)$ is used to control the impedance matching of the patch (LFIMP) at the lower frequency of operation and the width W_2 influences the impedance bandwidth at the lower frequencies. The major length (L_T) is chosen according to the following equation

$$L_T = L_2 + L_5 + L_6 + L_7 = \frac{c}{4f_L} \sqrt{\frac{2}{\epsilon_{\text{reff}} + 1}} \quad (5)$$

Table 1 lists the antenna parameters of the proposed design. This antenna was constructed and experimentally studied.

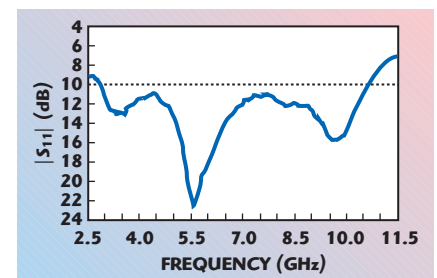


Fig. 2 Measured return loss of the proposed antenna.

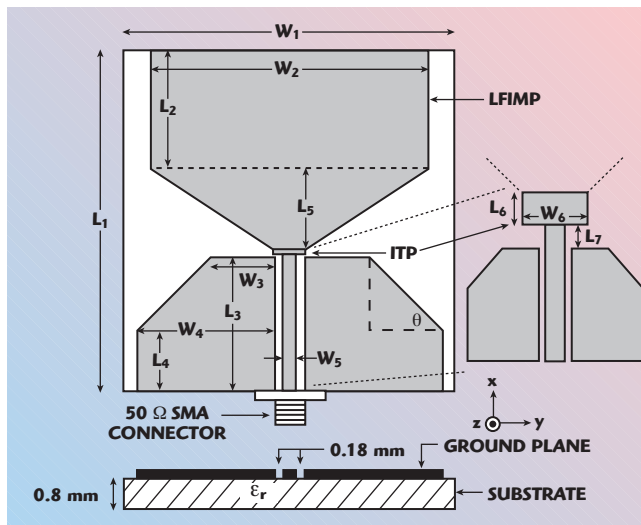


Fig. 1 Geometry of the printed CPW-fed UWB antenna.

TABLE I

DIMENSIONS OF THE CPW-FED RECTANGLE-TRAPEZOID-RECTANGLE MONOPOLE

Antenna Parameter	L_2	L_3	L_4	L_5	L_6	L_7	W_2	W_3	W_4	W_6	θ
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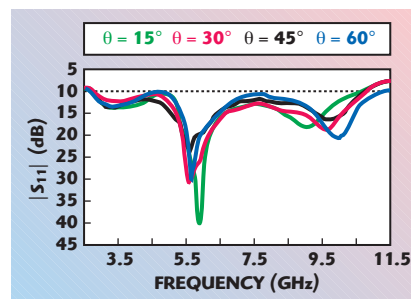
EXPERIMENTAL RESULTS AND DISCUSSION

To verify the performance of the proposed antenna, the prototype of the UWB antenna was measured after fabrication. The impedance bandwidth has been measured using the Agilent-8720ES vector network analyzer (VNA).

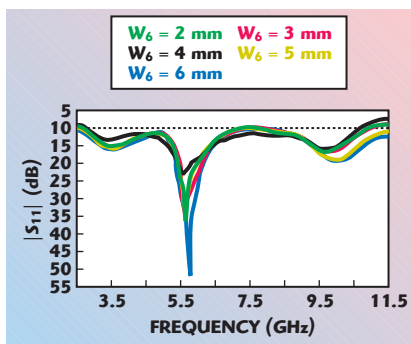
Figure 2 shows the measured return losses of the proposed antenna, which shows that a 10 dB bandwidth of 2.78 to 10.71 GHz has been achieved. The broadband of the rectangle-trapezoid-rectangle shaped monopole antenna is evident. This antenna has a matching impedance bandwidth that meets the requirements of the UWB band

of 3.1 to 10.6 GHz.

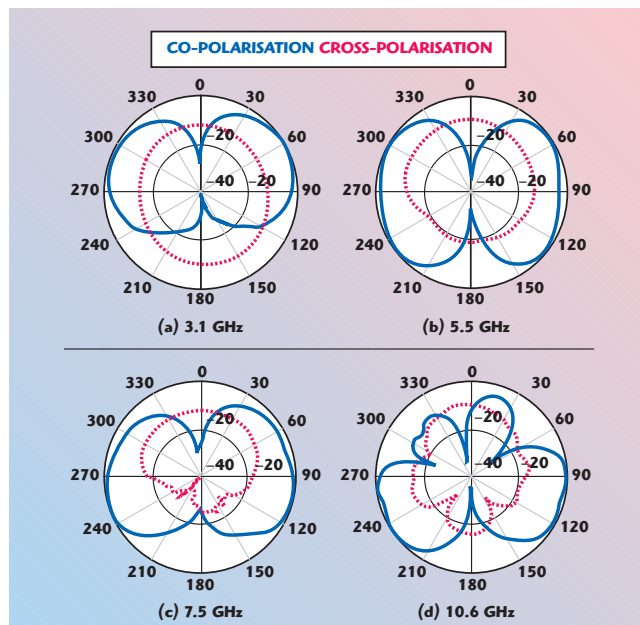
From the measured results shown, the length L_2 of the LFIMP is approximately 0.1 times the operating center wavelength. In **Figure 3**, the impedance bandwidth is measured as a function of θ when the other antenna dimensions, $L_1 = 31.45$ mm, $L_2 = 9.99$ mm, $L_3 = 14$ mm, $L_4 = 9$ mm, $L_5 = 6.61$ mm, $L_6 = 0.2$ mm, $L_7 = 0.65$ mm, $W_1 = 21.86$ mm, $W_2 = 19$ mm, $W_3 = 5$ mm, $W_4 = 10$ mm, $W_5 = 1.5$ mm, $W_6 = 4$ mm, $G_1 = 0.18$ mm, $h = 0.8$ mm and $\epsilon_r = 4.4$ are kept con-



▲ Fig. 3 Measured return loss as a function of the ground plane bevel angle.



▲ Fig. 4 Measured return loss as a function of W_6 .



▲ Fig. 5 Measured radiation patterns in the x - z plane (E-plane).

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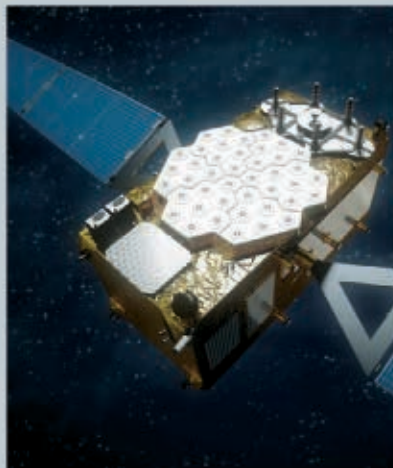
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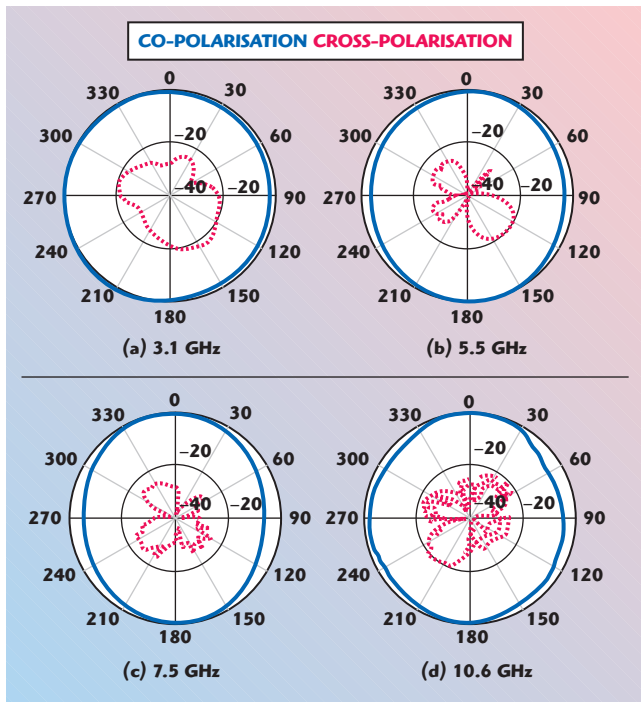
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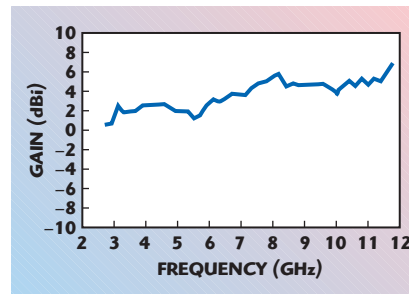
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▲ Fig. 6 Measured radiation patterns in the y-z plane (H-plane).

stant. It shows how the return loss of the rectangle-trapezoid-rectangle shaped monopole varies with different ground plane bevel angles θ . It can be observed that this



▲ Fig. 7 Measured gain of the proposed antenna.

arrangement of the design leads to the enhancement of the impedance matching bandwidth as the bevel angle θ increases. It is observed that the angle of θ determines the impedance matching in the band of 4 to 5.5 GHz.

Figure 4 shows the return loss for different ITP lengths (W_6), all other dimensions being identical to the previous figure. It is observed that the length of W_6 determines the impedance matching in the band of 6.5 to 9 GHz. The radiation patterns of the proposed antennas at 3.1, 5.5, 7.5 and 10.6 GHz were also measured. Figures 5 and 6 show the x-z plane (E-plane) and y-z plane (H-plane) patterns, respectively. It is obvious that the radiation patterns are nearly omni-directional patterns and suitable for UWB applications. Figure 7 shows that the measured antenna gain, within the operating frequency band, is 2.5 to 5.6 dBi. The gain flatness of the proposed antenna is suitable for UWB applications.

CONCLUSION

A novel CPW-fed printed rectangle-trapezoid-rectangle shape antenna has been proposed. The proposed

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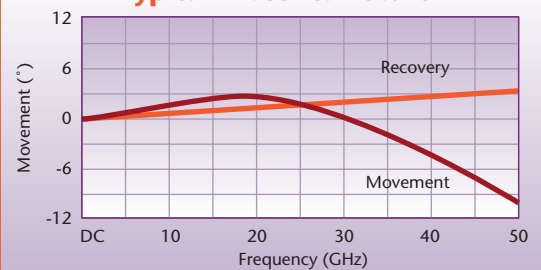
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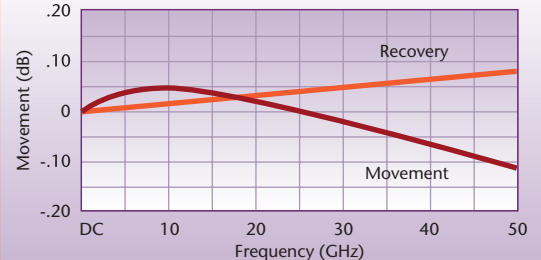
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antenna, with a compact size of $31.45 \times 31.45 \times 0.8$ mm, was implemented. It has a simple geometry, an effective feeding structure, an adequate operational bandwidth, a nearly smooth gain and has almost omni-directional radiation patterns. These features are very attractive for UWB applications and the antenna can be integrated in transceivers. ■

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ber of advantages including low cost, ease of handling and assembly, as well as suitability for mass production. Among these devices are unique, high linearity power amplifier technologies that house integrated power detectors and broadband, high performance receivers in small 4x4 mm packages.

MIMIX SMARTSET SOLUTIONS

Mimix recently launched its new "Mimix SmartSet" product line, which offers complete QFN chipset solutions to meet the requirements for next generation wireless communications. These Mimix SmartSet solutions give design engineers the ability to create complete SMT radio boards that can be manufactured by sub-contractors at very low prices and faster time to market, while still meeting the performance demands for higher linearity and

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- R & S ESIB26/40, FSP40, FSQ26/40, FSU26/40/50, FSUP26/40
- Discontinued** Advantest Agilent, Anritsu, IFR* & Tektronix models

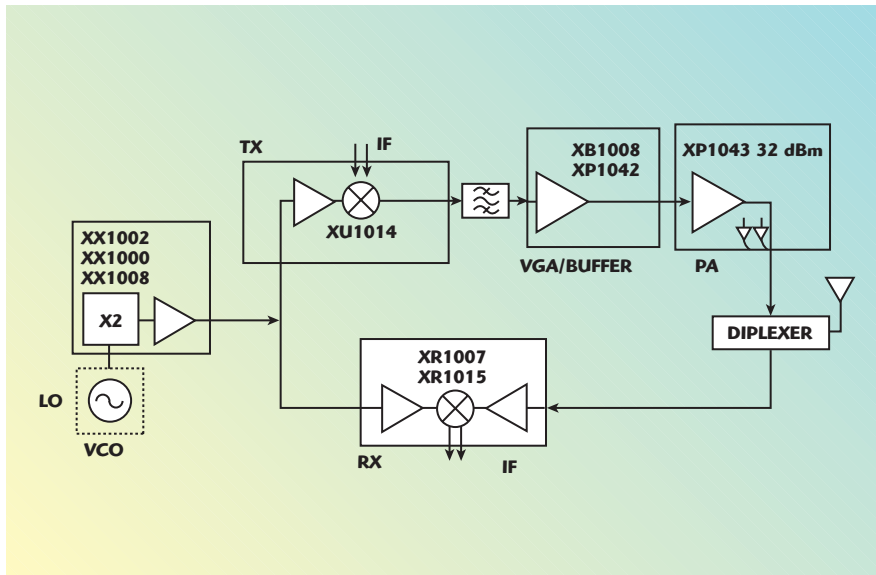
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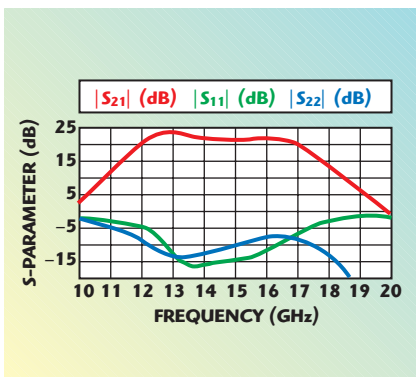
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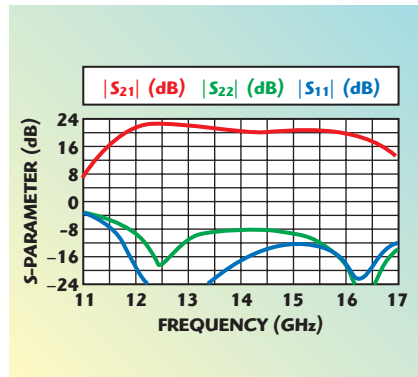
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▲ Fig. 1 Mimix 10 to 16 GHz chipset.



▲ Fig. 2 XP1042-QT small-signal parameter response vs. frequency ($V_{dd} = 5$ V, $I_{d1} = 125$ mA, $I_{d2} = 125$ mA, $I_{d3} = 250$ mA).



▲ Fig. 3 XP1043-QH small-signal response vs. frequency ($V_d = 7$ V, $I_{d1} = 60$ mA, $I_{d2} = 120$ mA, $I_{d3} = 240$ mA).

bandwidth applications. The key to this technology is the integration of four functions or more into a single MMIC, which reduces the chip-count, simplifies the design, minimizes the board layout, reduces cost and speeds up the design process. Therefore, these Mimix SmartSet QFN chipsets are ideally suited to meet the needs for next generation wireless communications design.

12 TO 16 GHz MIMIX SMARTSET

The Ku-band QFN Mimix chipset is shown in **Figure 1**. The block diagram is based on a common LO feed to the receive and transmit paths. On the receiver side, a single device, XR1015-QH, integrates an LNA, image reject mixer and LO buffer amplifier within a 4x4 mm standard

QFN package. The device includes on-chip ESD protection structures and DC-bypass circuitry to improve yields and ease handling during assembly. On the transmit path, the up-converter feeds into a buffer amplifier, XB1008-QT, which is a high gain, miniature device in a 3x3 mm QFN package. The buffer amp in turn feeds into a driver amplifier, XP1042-QT, followed by a power amplifier, the XP1043-QH. The XP1043-QH is the company's flagship product for the SmartSet chipset and it sets a new industry standard for performance for GaAs in a miniature 4x4 mm QFN package. The driver and PA pair can be bias adjusted to provide stable power and gain regulation over 30 dB of dynamic range with little degradation in the linearity performance.

Furthermore, the XP1043-QH PA includes a directional on-chip temperature compensated power detector for output power monitoring and gain power control mechanisms.

XP1042-QT "MINIATURE HIGH LINEARITY DRIVER AMPLIFIER"

The 12 to 16 GHz driver amplifier, XP1042-QT, is offered in a 3x3 mm QFN package and offers superior power handling and linearity. The device delivers high performance with 38 dBm OIP3, 25 dBm P1dB and 21 dB gain. **Figure 2** shows small signal parameter response over the frequency range. The device is highly efficient requiring only 5 V and 500 mA to provide high linearity with 38 dBm OIP3. The bias can be controlled to achieve linear gain control by reducing the drain current. This lower drain current also improves the DC power consumption of the radio in the turn-down mode. The unique offering for this product is the very high IP3 to P1dB ratio of 13 dB, which makes the device an ideal candidate for very high linearity driver applications.

XP1043-QH "HIGH LINEARITY AND DC EFFICIENCY WITH POWER DETECTION"

The 12 to 16 GHz power amplifier, XP1043-QH, is the Mimix SmartSet flag-ship product. The device is offered in a standard 4x4 mm QFN package and offers a set of unique features making it ideally suited to large volume linear radio requirements. Firstly, it provides 30 dBm P1dB and 41 dBm OIP3 in the linear, DC efficiency mode with 5 W DC power consumption. **Figure 3** shows the small signal response over the frequency range, which shows that the packaged device has greater than 20 dB gain and is fully matched across the band. The device is also rated to be biased up to 10 V and 1000 mA, which enables it to provide over 2 W of saturated RF power. The XP1043-QH also includes an on-chip temperature-compensated power detector and offers power and gain control through bias adjustment. The integrated power detector allows the user to control the linear output power without needing to use a discrete power detector and attenuator, and



Solid State Tetrode Tube and Combination Amplifiers

Model Number	Freq Range (MHz)	Min Pwr Out (Watts)	Min Sat Gain (dB)
M/TCCX/SCCX Series • .01-220 MHz			
SCCX300	.01-220	300	55
SCCX500	.01-220	500	57
M404	.01-220	500	57
M406	.01-220	1000	60
TCCX2000	.01-220	2000	63
TCCX2200	.01-220	2200	63
TCCX2500	.01-220	2500	64

CMX/SMX Series • .01-1000 MHz			
SMX301	.01-1000	300/100	55/50
SMX302	.01-1000	300/200	55/53
SMX303	.01-1000	300/300	55/55
SMX501	.01-1000	500/100	57/50
SMX502	.01-1000	500/200	57/53
SMX503	.01-1000	500/300	57/55
CMX10001	.01-1000	1000/100	60/50
CMX100010	.01-1000	1000/1000	60/60

Microwave Solid State and TWT Amplifiers

Model Number	Freq Range (GHz)	Min Pwr Out (Watts)	Min Sat Gain (dB)
T-200 Series • 200-300 Watts CW 1-21.5 GHz			
T251-250	1-2.5	250	54
T82-250	2-8	250	54
T188-250	7.5-18	250	54
T2118-250	18.0-21.7	250	54

T-500 Series • 500 Watts CW 1-18 GHz			
T251-500	1-2.5	500	57
T7525-500	2.5-7.5	500	57
T188-500	7.5-18	500	57

MMT Series • 5-150 Watts, 18-40 GHz			
T2618-40	18-26.5	40	46
T4026-40	26.5-40	40	46

S/T-50 Series • 40-60 Watts CW 1-18 GHz			
S21-50	1-2	50	47
T82-50	2-8	50	47
T188-50	8-18	50	47

Solid State Amplifiers

Model Number	Freq Range (MHz)	Min Pwr Out (Watts)	Min Sat Gain (dB)
SMCC Series • 200-1000 MHz			
SMCC350	200-1000	350	55
SMCC600	200-1000	600	58
SMCC1000	200-1000	1000	60
SMCC2000	200-1000	2000	63

SMC Series • 80-1000 MHz			
SMC250	80-1000	250	54
SMC500	80-1000	500	57
SMC1000	80-1000	1000	60

SMX-CMX Series • .01-1000 MHz			
SMX100	.01-1000	100	50
SMX200	.01-1000	200	53
SMX500	.01-1000	500	57

SVC-SMV Series • 100-1000 MHz			
SVC500	100-500	500	57
SMV500	500-1000	500	57

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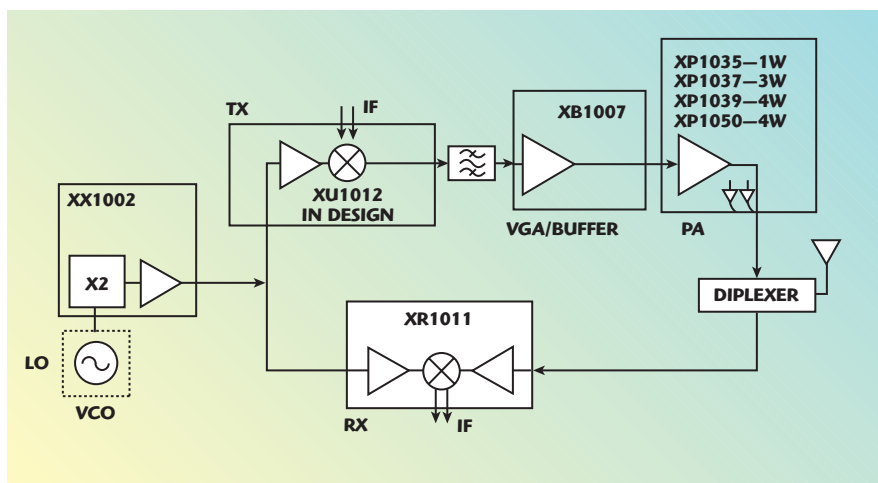
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Frequency Bands						
L	S	C	X	Ku	K	Custom
LNAs	✓	✓	✓	✓	✓	✓
SSPAs	✓	✓	✓	✓	✓	✓
LNBS			✓			✓
BUCs			✓			✓

✓ = New

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PRODUCT FEATURE



▲ Fig. 4 Mimix 5 to 10 GHz QFN chipset.

this enhanced functionality simplifies the design requirements and lowers cost for transmit applications.

5 TO 10 GHz MIMIX SMARTSET

The 5 to 10 GHz QFN chipset is shown in **Figure 4** with a common LO feed configuration. On the receiver side, a single device, XR1011-QH, integrates an LNA, image reject mixer and LO buffer amplifier within a 4x4 mm standard QFN package. The device includes unique active on-chip ESD protection structures, which are 'disabled' once the device is biased up for use. During handling and assembly, the ESD structures actively shunt possibly damaging static charge away from the most sensitive circuit structures. Furthermore, the device has sufficient DC-bypass circuitry to simplify the board layout and bias design. On the transmit path the RF is fed into a buffer amplifier, XB1008-QT, which is a high gain, miniature device in a 3x3 QFN package. The buffer amplifier in turn feeds into a driver amplifier with 29 dBm P1dB, XP1035-QH, followed by a number of options for high power linear amplifiers, which deliver up to 4 W of saturated RF power and 50 dBm OIP3. The high power amplifiers (HPA) employ HFET GaAs technology, which provides high power and linearity at high DC efficiencies and increased thermal reliability, allowing these devices to be offered in standard 6x6 mm QFN packages. These new 4 W devices are the industry's first fully molded 6x6 mm QFN power amplifier MMICs that provides a viable alternative to discrete power FETs.

XR1011-QH "HIGH PERFORMANCE BROADBAND OPERATION"

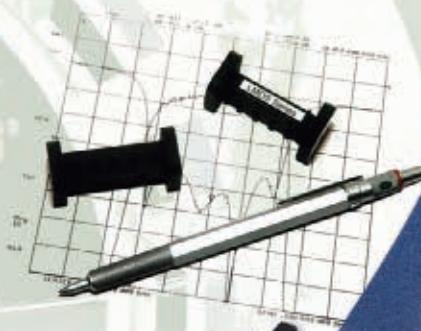
The XR1011-QH is the industry's first fully molded 4x4 mm QFN packaged receiver covering the frequency range of 4.5 to 10.5 GHz. The part is distinguished by its high performance; combining low noise figure, high conversion gain and excellent linearity across the entire band. The device integrates an image reject mixer, an LO buffer amplifier, and a low noise amplifier within a fully molded 4x4 mm QFN package that is RoHS compliant. ESD protection structures and DC-bypass are all included on-chip to provide high yields and ease the handling, board design and implementation in assembly. The conversion gain is shown in **Figure 5**. The NF shows very good performance across the band with better than 2 dB at room temperature and little variation in temperature from -40° to +85°C. The device offers high conversion gain of 14 dB and IIP3 of +3 dBm, making it a market leader in integrated, packaged receiver technology.

XP1035-QH "VERSATILE BROADBAND POWER AMPLIFIER"

The XP1035-QH is a packaged linear power amplifier that operates over the 5.9 to 9.5 GHz frequency band. The device provides high gain of 26 dB gain (see **Figure 6**) and linearity of 39 dBm OIP3 across the band. The packaged amplifier is comprised of a three-stage power ampli-



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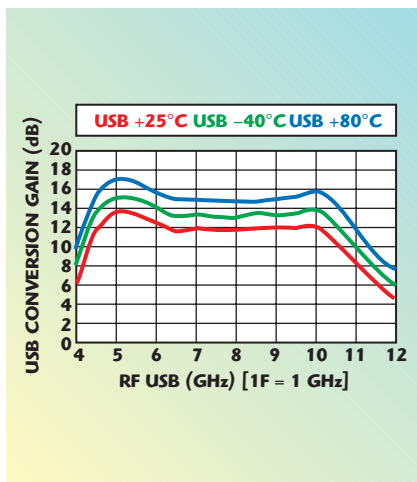
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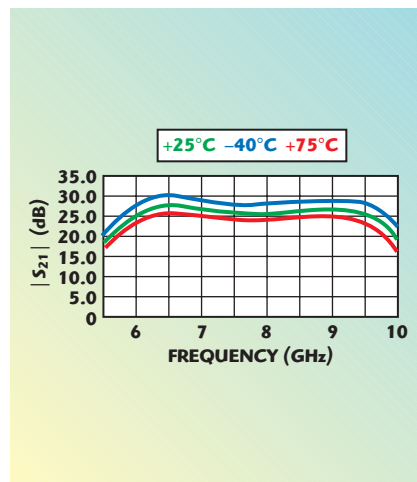
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PRODUCT FEATURE



▲ Fig. 5 XR1011QH USB conversion gain (4 V @ 130 mA, $P_{LO} = 5$ dBm).

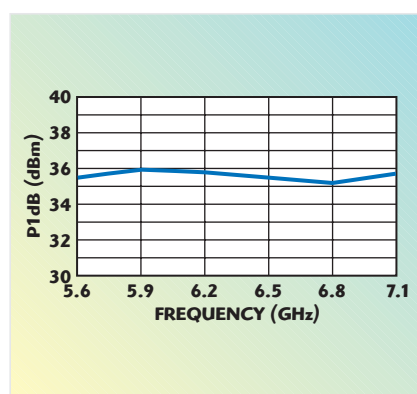


▲ Fig. 6 XP1035-QH gain vs. frequency ($V_d = 6$ V, $I_d = 500$ mA).

er with an integrated, temperature compensated on-chip power detector and is offered in an industry standard, fully molded 4x4 mm QFN package. The device includes on-chip ESD protection structures and DC bypass capacitors to ease the implementation and volume assembly of the packaged part. The combination of broadband performance and strong drive level with standard QFN packaging make the device highly versatile for a wide range of applications.

XP1039-QJ "4 W POWER IN STANDARD QFN PACKAGE"

Mimix now offers very high linearity packaged power amplifiers for the 5.6 to 8.5 GHz frequency bands in standard 6x6 mm QFN packages. These new devices are the industry's first high power amplifiers in standard 6x6 mm packages and present an attractive alternative to discrete power FETs due to some key advantages. Firstly, the devices provide plenty of linearity with up to 50 dBm OIP3 using HFET wafer technology and they operate at lower DC power consumption levels. Secondly, the devices are high gain with up to 16 dB gain, thus greatly reducing the power requirements for driver amplifiers and hence lowering DC power consumption and overall BOM cost. Thirdly, the components are fully matched and broadband in performance, which further reduces the BOM count and simplifies the board design. Finally, the power amplifiers are offered in standard 6x6 mm QFN



▲ Fig. 7 XP1039-QJ P1dB vs. frequency ($V_d = 8$ V, $I_d = 1400$ mA).

packages, an industry first to offer such high linearity and power with all the advantages associated with standard QFN packaging. The gain of the XP1039-QJ is greater than 16 dB from 5.6 to 7.1 GHz and **Figure 7** shows the P1dB performance as a function of frequency, which shows the device is capable of delivering up to 4 W of RF power at P1dB.

Mimix Broadband has developed Mimix "SmartSets" for the bands between 5 to 16 GHz and chipsets for the 16 to 32 GHz band are in development. These Mimix SmartSet QFN chipsets are ideally suited to meet the needs for next generation wireless communications design.

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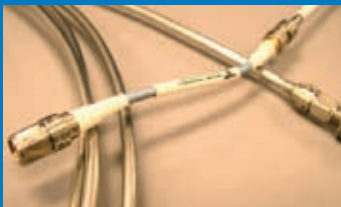
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MID-RANGE VECTOR SIGNAL GENERATOR WITH INTERNAL SIGNAL GENERATION

The world of telecommunications has experienced an accelerated period of change in recent years. In the past, many terminals such as mobile telephones and PDAs were only capable of transmitting and receiving signals based on a few different standards such as GSM and WCDMA. However, increasing numbers of functions and standards are now being integrated into terminal equipment (e.g. GSM, WCDMA, WLAN, WiMAX, GPS, FM radio and mobile TV).

In addition, the data rate to be transmitted has increased from a few kbit/s in GSM to target data rates of 100 Mbit/s in LTE, while the transmission bandwidth has grown from several hundred kHz to as much as 40 MHz in 802.11n. Modulation methods such as OFDM/OFDMA and other techniques such as MIMO have found a place in all of the new communications standards.

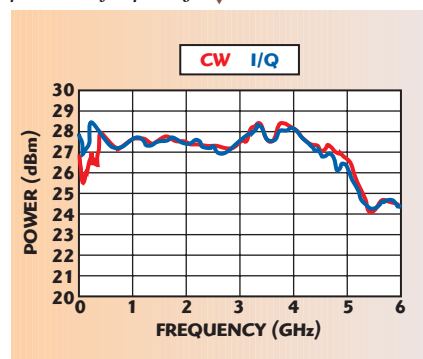
All of these advances are presenting new test and measurement challenges. For in-

stance, developing and manufacturing equipment requires signal generators with all-round qualities and the capability of keeping up with the rapid development of modern technology. However, such generators must also be scalable so that users only have to invest what is necessary to meet their current test requirements.

It is a tough task for a mid-range vector signal generator to satisfy all of these different criteria, but the new, compact R&S SMBV100A vector signal generator is up to the challenge. Its RF characteristics are paired with a flexible baseband architecture and many useful add-on functions.

It is available for frequency ranges from 9 kHz to 3.2 GHz or from 9 kHz to 6 GHz. The vector signal generator is characterized by high output power of typically +24 dBm across its entire frequency range (see **Figure 1**). This is particularly advantageous with complex test set ups. Components such as cables, switches and couplers often cause significant

Fig. 1 Measured maximum output power vs. frequency. ▼



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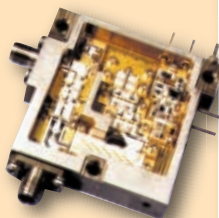
CTT offers not only form, fit, function of microwave amplifier replacements for many mature systems, but also incorporates leading-edge technology components such as GaN and SiC.

CTT is well positioned to offer engineering and production technology solutions — including high-rel manufacturing — to infuse new technology into legacy systems for improved reliability and life cycle costs.

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TABLE I
APPLICATION-SPECIFIC BASEBAND CONFIGURATION

Baseband Option	Baseband Generator	RF Bandwidth	Recommended Use
R&S SMBV-B10	Baseband coder with realtime functionality and ARB (32 Msample or 256 Msample)	120 MHz	R&D, service
R&S SMBV-B50	ARB only (32 Msample or 256 Msample)	120 MHz	Production
R&S SMBV-B51	ARB only (32 Msample or 256 Msample)	60 MHz	Production

TABLE III
SPECIFICATIONS IN BRIEF

Frequency		
Frequency range	R&S SMBV-B103/R&S SMBV-B106	9 kHz to 3.2 GHz/6 GHz
Setting time	SCPI mode, ALC state ON, CW mode	<3 ms
	List mode	<1 ms
Power Level		
Maximum output power	1 MHz < f ≤ 6 GHz	>+18 dBm (PEP)
Setting time	SCPI mode, ALC state ON, CW mode	<2.5 ms
	List mode	<1 ms
Spectral Purity		
Harmonics	f > 1 MHz; CW, level ≤ 8 dBm	<−30 dBc
Non-harmonics	CW, level > −10 dBm, >10 kHz carrier offset, f ≤ 1500 MHz	<−70 dBc (nominal <−85 dBc)
SSB phase noise	f = 1 GHz, 20 kHz carrier offset, 1 Hz measurement bandwidth, CW	<−122 dBc (nominal −128 dBc)
Wideband noise	attenuator mode AUTO CW, level > 5 dBm, >10 MHz carrier offset, 1 Hz measurement bandwidth	<−142 dBc (nominal −152 dBc)
Supported Analog Modulation Modes		
AM/FM/PM		standard
Maximum FM/φM deviation	f > 3 GHz	16 MHz/160 rad
Pulse modulation		optional with R&S SMBV-K22
On/off ratio		>80 dB
Rise/fall time	10% to 90% of RF amplitude	<20 ns, typ. 4 ns
Minimum pulse width	using the optional R&S SMBV-K23 pulse generator	10 ns
I/Q Modulation		
ACLR	WCMDA 3GPP FDD, TM 1/64	typ. 67 dBc
EVM	WCMDA 3GPP FDD, TM 1/64	typ. 0.6%
	WiMAX IEEE 802.16e	typ. 0.4%
	EUTRA/LTE	typ. 0.4%

TABLE II
SELECTION OF INTERNALLY SUPPORTED SIGNALS (WITH ADDITIONAL OPTIONS)

3GPP FDD including HSPA/HSPA+
TD-SCDMA
CDMA2000® ¹
1xEV-DO
EUTRA/LTE (FDD+TDD)
GSM/EDGE
WiMAX
WLAN IEEE 802.11a/b/g/n
DVB-H/DVB-T
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¹ CDMA2000® is a registered trademark of the Telecommunications Industry Association (TIA – USA)
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power loss that requires adequate compensation. With the R&S SMBV100A, the use of external amplifiers can be avoided. This minimizes the overall uncertainty of the test set up and helps to avoid additional costs.

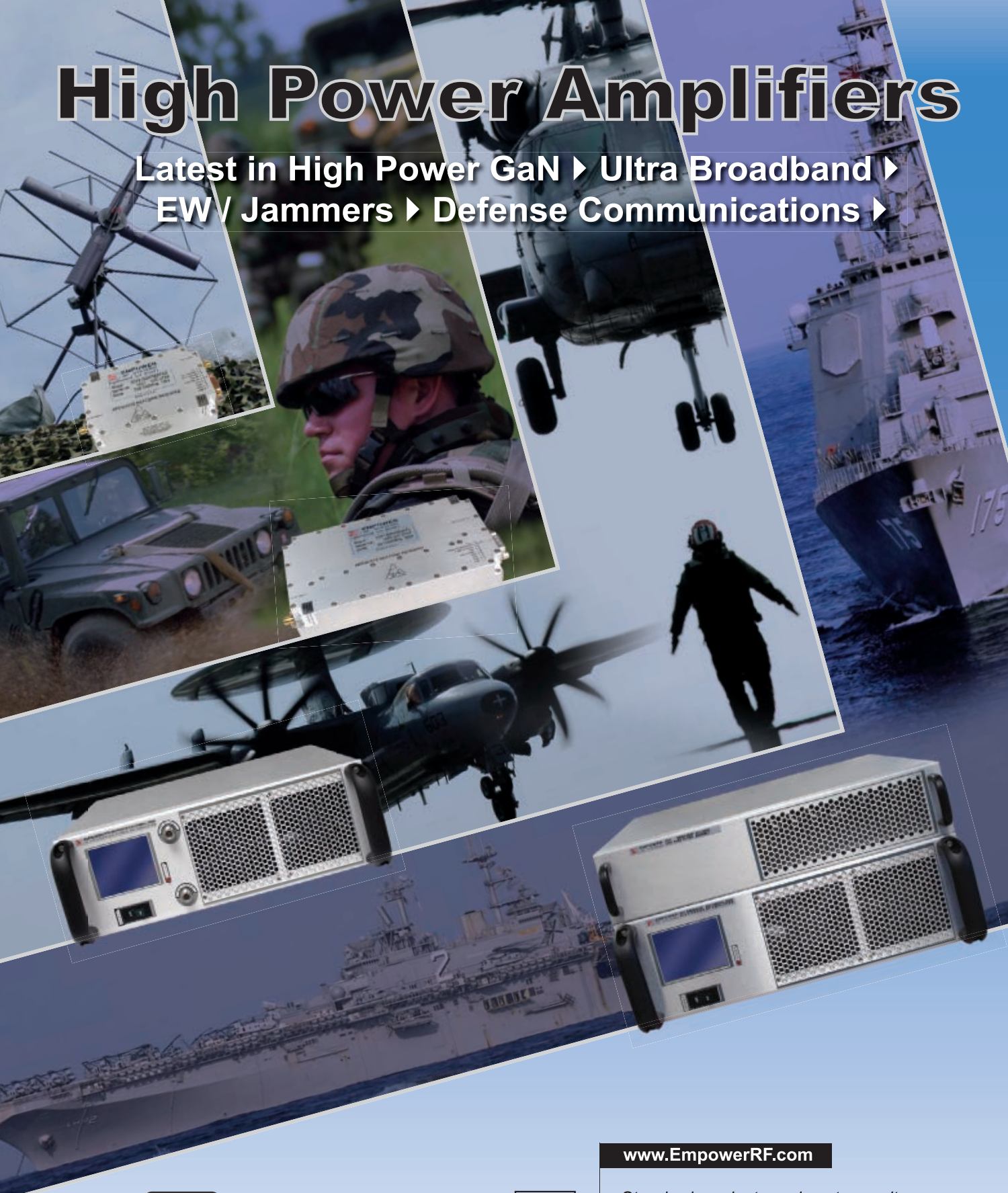
The new instrument also offers very good signal purity. The SSB phase noise has a nominal value of 128 dBc/Hz (20 kHz offset) at f = 1 GHz (see **Figure 2**). Non-harmonics undergo nominal suppression of better than 85 dB and the wideband noise has a nominal value of 152 dBc. The error vector magnitude (EVM) for signals such as WiMAX IEEE 802.16e and LTE is typically 0.4 percent, while the level repeatability has a nominal value of 0.05 dB.

MODULATION BANDWIDTH UP TO 528 MHZ

Today's communications standards require more and more transmission bandwidth to handle the growing complexity of multimedia applications and the R&S SMBV100A is well equipped to

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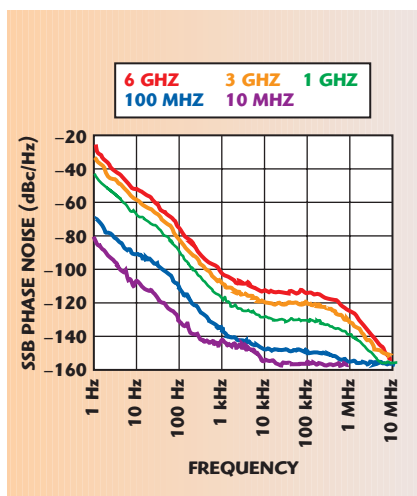
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meet the challenge. With internal signal generation, RF bandwidths of 60 or 120 MHz can be selected. Even multicarrier signals for wide-band wireless communications standards such as WLAN IEEE 802.11n and LTE can be generated.

With external I/Q modulation, the maximum RF modulation bandwidth of the R&S SMBV100A is 528 MHz. This allows up-conversion of UWB signals, which can be generated using the R&S AFQ100B baseband generator (see **Figure 3**, for example). At the same time, the large I/Q bandwidth ensures high time resolution for the signals.

Very fast baseband frequency hopping as used in military applications and generation of steep-edged radar pulses with complex modulation are thus feasible in conjunction with an external I/Q source such as the R&S AFQ100B. Thus, the R&S SMBV100A can replace more expensive vector signal generators, which are utilized solely for their large bandwidth and not any other capabilities.



▲ Fig. 2 Measured SSB phase noise with internal OCO (R&S SMBV-B1 option).

CUSTOMIZED INTERNAL SIGNAL GENERATION

Customizing test instruments to fit the application is more or less a standard practice nowadays. However, the R&S SMBV100A implements this feature in an unusual way, being unique in its class by being equipped

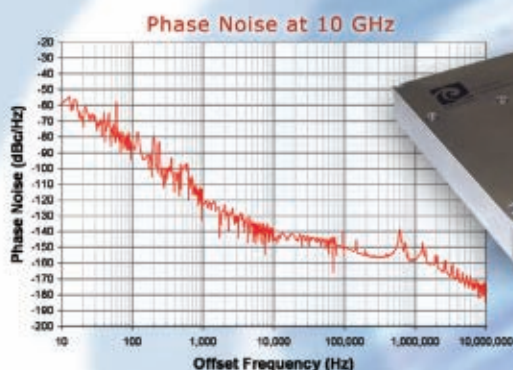
with a real time baseband coder for direct signal generation.

Alternatively, it allows selection between different versions of an arbitrary waveform memory from which pre-calculated waveforms can be played back. This means that a single platform can provide a solution that can be optimally adapted to requirements in production and development.

In production applications, standardized test sequences are required along with fast frequency and level setting times that the R&S SMBV100A also ensures with a value of <1 ms in the List mode. For playing back these test signals (which are generally pre-calculated), a total of four different versions of the arbitrary waveform memory (ARB) are available. Depending on the configuration, the instrument offers a bandwidth of 60 MHz or 120 MHz and an I/Q memory size of 32 Msamples or 256 Msamples (see **Table 1**).

This makes it possible to easily play back even long test sequences, which is a requirement for digital radio standards, for example. Addition-

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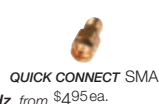
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S4W2	S4W5	N4W5	4	±0.40
S5W2	S5W5	N5W5	5	±0.40
S6W2	S6W5	N6W5	6	±0.40
S7W2	S7W5	N7W5	7	-0.4, +0.9
S8W2	S8W5	N8W5	8	±0.60
S9W2	S9W5	N9W5	9	-0.4, +0.8
S10W2	S10W5	N10W5	10	±0.60
S12W2	S12W5	N12W5	12	±0.60
S15W2	S15W5	N15W5	15	±0.60
S20W2	S20W5	N20W5	20	-0.5, +0.8
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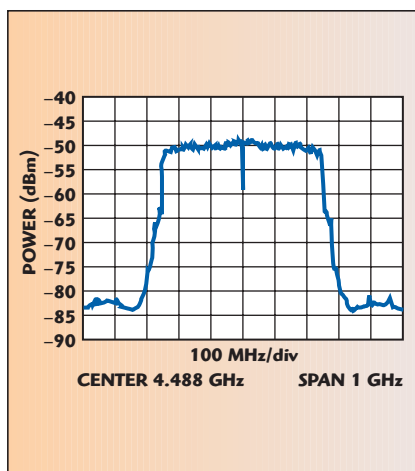
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ally, the large I/Q memory enables the storage of different signals as part of a multi-segment waveform and switching between the individual signals in just a few microseconds. This is especially useful during production tests on multi-standard modules that are designed to support a wide variety of digital standards, e.g. GSM and UMTS. The test signals can be pre-calculated using either the R&S WinIQSIM2 signal generation software or third-party programs.

In research and development environments, the R&S SMBV100A is useful due to its optional real time baseband coder. Test signals for all major digital communications standards can be configured directly on the instrument (see **Table 2**). Users can also avoid the hassle of having to pre-calculate the signals on an external PC and transfer them to the signal generator. This makes it possible to modify individual parameters quickly and easily while directly examining the effects on the device under test. Everyday work in the lab is accelerated, helping to shorten



▲ Fig. 3 Frequency response of the IQ modulator with a bandwidth of > 500 MHz.

development time and design cycles.

The real time coder also enables generation of infinitely long test sequences, e.g. for simple digitally modulated signals as well as for internally generated digital standards such as GSM/EDGE and 3GPP FDD (downlink). Such long test sequences

serve as a reliable basis for performing bit error rate tests, particularly in cases where long bit sequences are needed to ensure statistically meaningful results.

A TRUE ALL-ROUNDER

A signal generator is only as good as its interfaces. This applies to the interfaces for connecting to the device under test, for synchronizing with different test instruments and for handling remote control, as well as to the user interface itself.

In addition to the RF interface, the R&S SMBV100A also includes analog differential I/Q outputs as a standard feature, while an optional digital I/Q output will be available in the first quarter of 2009 (enabled via software). This makes the vector signal generator suitable for tests at the RF and in the baseband.

For the baseband generator, a wide range of trigger and marker functions are available to ensure accurate synchronization with the device under test. In the RF range, multiple signal generators can be



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interconnected using the phase coherence option. Usage of a common local oscillator (LO) signal ensures the phase coherence needed to make, for example, measurements on phased-array antenna systems (beamforming) or components with differential RF (e.g. amplifiers).

In the area of remote control, the instrument meets all needs; USB, LAN and GPIB interfaces are available along with the appropriate software drivers. An integrated VNC server also enables convenient remote control of the instrument via a web browser.

The R&S SMBV100A is Rohde & Schwarz' first vector signal generator that uses Linux as its operating system, which helps to safeguard against viruses. Passwords can be set or the USB interfaces in the instrument can be disabled if necessary. The instrument also offers an optional removable 80 GB hard disk, which is useful for keeping critical data secure while being able to transport the instrument as required. This helps to avoid costly sanitizing procedures otherwise needed before an instrument can be removed from a secure area. If required, however, sanitizing can be performed easily.

The R&S SMBV100A also incorporates a convenient user interface that will be familiar from the company's other signal generators. The block diagram enables intuitive operation while the integrated transient recorder (graphics block) enables visual monitoring of the signals that are generated (I/Q diagram, spectrum, constellation, CCDF, eye diagram, etc.). The context-sensitive online help facility provides useful background information about all setting parameters of the signal generator.

CONCLUSION

When designing a new all-round vector signal generator, the trick is to meet today's requirements while also leaving room to satisfy future requirements and the R&S SMBV100A provides sufficient reserves. It combines the benefits of purely analog signal generators with those of a powerful vector signal generator. The instrument contains features that are normally only found in high-end signal generators (see **Table 3**). At the same time, it offers a good price/performance ratio. This is due to the three-year calibration cycle, the high-quality technical implementation and the user-friendly service concept that makes it possible to quickly repair instruments on-site if necessary.

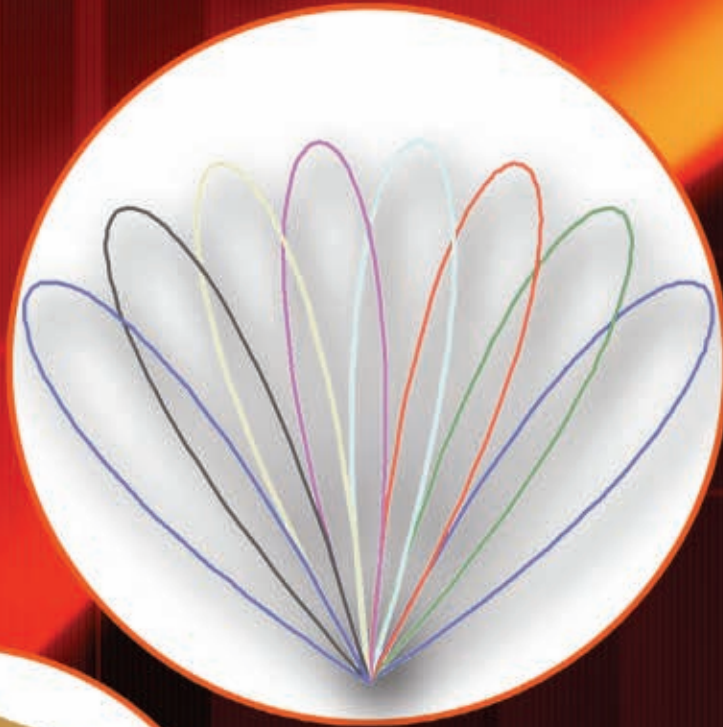
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EFFICIENT, ACCURATE, RELIABLE EM SIMULATION TOOL

In the ongoing race for reduced design costs and faster time to market, simulation efficiency remains the most important factor in electromagnetic field analysis. Simulation efficiency can be determined by the time taken to reach the final design, which is strongly influenced by the level of workflow integration, the versatility in manipulating the model, the choice of solver type, the method's accuracy, the implementation's efficiency and, of course, the hardware speed. The new CST STUDIO SUITE™ 2009, incorporating the CST MICROWAVE STUDIO® (CST MWS) 3D electromagnetic field simulator for microwaves and RF, has been specifically designed to meet these requirements.

USABILITY

For this new version, the modeling interface has undergone a complete makeover. Besides changes that simplify user access to functionality, there are improvements in user interaction. Transformations such as translation, rotation and scaling can now be performed using mouse control. In addition, version 2009 features a special interactive alignment mode that allows geometrical objects in

the model to be positioned easily with a few mouse clicks. The new alignment mode is automatically activated when copying objects between two projects by standard copy [Ctrl-c] and paste [Ctrl-v] operations, or when importing sub-projects into the main project.

Conformal modeling is often required, particularly for antenna applications. Version 2009 offers an interactive bending feature. **Figure 1** shows the 3D model of an antenna carrier. The antenna itself is modeled as a planar structure, which is then imported in a separate step. The two objects are aligned (see Figure 1; top), then the bending process is started by selecting individual faces (see Figure 1; middle, highlighted red) of the carrier onto which the antenna should be bent. Eventually the entire antenna is fitted perfectly to the carrier (see Figure 1; lower). This is actually very similar to the real procedure, where the antenna is printed onto a flexible foil and then attached to the carrier.

Perhaps the most important among all the improvements to the modeling front-end is

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not visible at all; the entire user interface has been ported to 64-bit in order to serve the demand for dealing with increasingly complex models.

INTEROPERABILITY

Workflow integration has always been a key concern in CST's development. All import filters available in the CST STUDIO SUITE are characterized by their robustness and ability to deal with flaws in the im-

ported models. Besides updating the CAD kernel and the existing import filters, the palette of available imports/exports is being continuously extended. Version 2009 now features Nastran, GDSII and Gerber exports.

Particular attention has been directed to the imports from EDA tools, e.g. from Cadence®, Mentor Graphics® and Zuken®, since the investigation of signal integrity is becoming an increasingly important application area for 3D EM simulation. These EDA interfaces can also deal with importing lumped circuit components. A completely new feature is the Mentor Graphics PADS® import.

SIMULATION PERFORMANCE

Computers are getting faster every year. But while CST has seen a performance increase for desktop workstations of about a factor 25 for a simple scalar textbook FDTD implementation in the last 10 years, the increase in average model complexity is actually greatly outweighing this. Factor increases of 1000 in numerical model size are not uncommon (see **Figure 2**). For a mobile phone simulation, 10 years ago it was acceptable to replace the actual mobile phone by a metallic block and focus on the antenna. Today the entire mobile phone, its antennas, PCB, cameras, etc., have to be simulated, while also considering the presence of the phone user's head, hand, perhaps even the entire body, and the environment it is in.

Improvements in both the algorithms and hardware concepts must be leveraged. The neglect of one of these aspects necessarily leads to decreased performance. On the algorithmic side, CST takes the complete technology approach. An Allen screw can be tightened much quicker with an Allen key than with any other kind of screwdriver. Similarly, users can choose the tool within CST MWS that best suits their application.

On the next level, technologies like the Perfect Boundary Approximation (PBA)®, the Thin Sheet Technology (TST)™ and the Multilevel Subgridding Scheme (MSS)™ can improve performance dramatically. Improvements in implementation have also led to significant performance gains in the frequency domain solver.

Improvements on the hardware side are taking place at various levels.

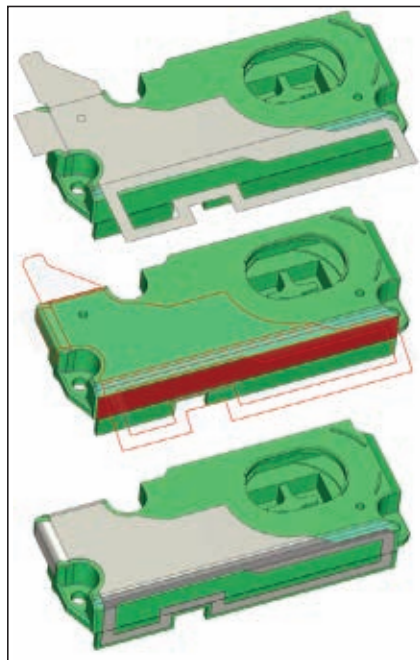
Together with Intel®, performance on desktop workstations has been further improved. In collaboration with Acceleware, GPU-based hardware acceleration has been made available to CST MWS users. Currently one-, two- and four-card solutions are available. Compared to high-end desktop workstations, speed-ups of up to a factor 19 have been achieved for typical applications. The upcoming realizations of GPU-based hardware acceleration using Nvidias Compute Unified Device Architecture (CUDA) programming language promise further performance improvements.

MPI FOR CST MWS

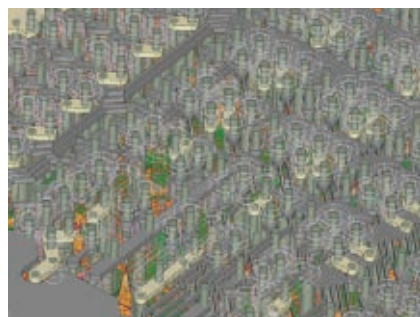
Hardware acceleration solutions for CST MWS are currently limited to a maximum of 96 million mesh nodes. Very complex structures such as multilayered PCB boards or electrically large models can easily exceed this limit. They will benefit most from the company's latest development: A message passing interface (MPI)-based parallelization of the CST MWS transient solver. By decomposing the calculation domain into several parts and distributing these parts to computers in a cluster, the simulation of models with several hundreds of millions of mesh nodes becomes feasible. At the same time the simulation is sped up by using several CPUs and memory interfaces in each individual computer.

TRUE SURFACE MESH ADAPTATION

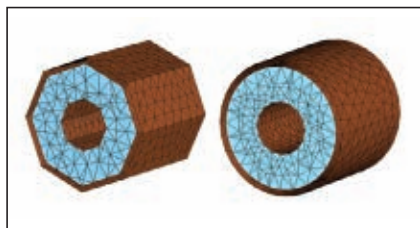
As an additional algorithmic advance, the mesh adaptation of CST MWS's tetrahedral frequency domain solver has been entirely revised. Traditionally, adaptive refinement of HF frequency domain solvers based on a tetrahedral grid does not improve on the initial faceted representation of the structure. The originally created tetrahedra are simply divided further where necessary. The mesh adaptation will converge, not to the results of the actual structure (e.g. S-parameters), but to those of the initial segmented model (see **Figure 3**; left). CST's mesh adaptation approach is different. After every adaptation step the proposed refinement is projected back onto the original model. This leads to an improved geometry approximation and to a convergence to the real results of this structure (see **Figure 3**; right).



▲ Fig. 1 Interactive bending of a fictitious antenna onto a carrier.



▲ Fig. 2 Complex EDA import for signal integrity analysis.



▲ Fig. 3 Coaxial waveguide after traditional (left) and true surface (right) mesh adaptation.



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INTEGRAL EQUATION SOLVER

Introduced for the solution of electrically large structures in CST MWS version 2008, the integral equation solver, based on the multilevel fast multipole method (MLFMM), is catching up with the rest of the company's solvers with respect to available features. The performance improvements over the previous version are dramatic. Besides MLFMM, an iterative MoM solver is available for solv-

ing structures that are electrically not very large, i.e. in the range of about 5 to 20 wavelengths. The memory efficiency is also good ($N \log(N)$ compared to N^3 for normal MoM).

TRUE TRANSIENT EM/CIRCUIT CO-SIMULATION

Particularly beneficial for engineers working in signal integrity, CST STUDIO SUITE 2009 additionally features true transient EM/circuit co-simulation.

In standard EM/circuit co-simulation, the circuitry and 3D structures are solved separately, and S-parameter models represent the 3D EM structure in a circuit simulator [e.g. CST DESIGN STUDIO™ (CST DS)], which then solves the entire set-up.

CST MWS models, for example, can also be used within Agilent ADS or AWR Microwave Office. Although this is not co-simulation in the sense that 3D EM fields and circuit components influence each other, it is very useful to analyze and optimize a system in a way that also accounts for full 3D effects.

The new scheme available in version 2009 follows a different path, although the principal set-up looks very similar. A full 3D structure is represented by a block in a schematic, and circuit components are attached to its ports. The transient 3D EM/circuit co-simulation exchanges currents and voltages continuously at the ports between the CST MWS EM simulation and the circuit simulation in CST DS, while the signal propagates through the model (see **Figure 4**).

There are two major advantages of transient compared to standard EM/circuit co-simulation:

- The full S-matrix of the 3D EM structure is no longer required since the circuit elements are directly interacting with the electromagnetic field simulation. This is advantageous particularly for PCBs with many ports and many lumped elements because the full S-matrix derivation of such a device can be extremely time consuming and is not always necessary for the investigation of critical parts.
- Transient EM/circuit co-simulation can also simulate the transient electromagnetic fields that result from the interaction with non-linear elements such as diodes. The broadband nature of the transient simulation means that many harmonics are automatically taken into account (see **Figure 4**).

TRANSIENT THERMAL SIMULATION

The thermal analysis of electromagnetic losses is a natural augmentation of EM simulation tools. In previous versions, a stationary heat equation solver was available. In version 2009 its capabilities are extended to simulate the transient behavior of the heating process. For the benefit of



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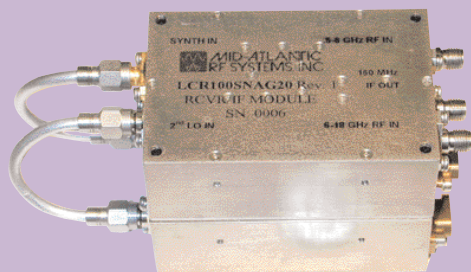
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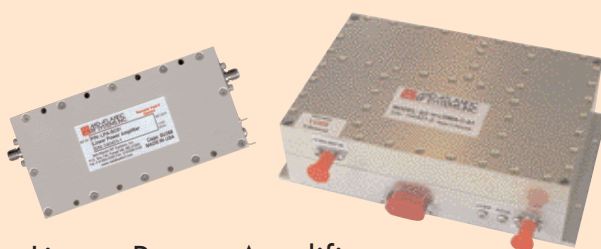


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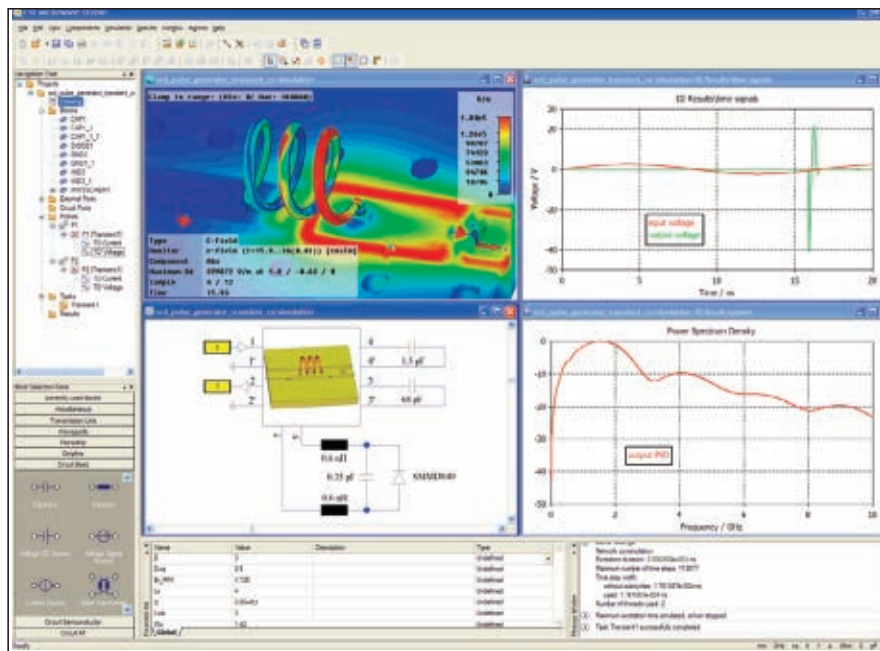
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▲ Fig. 4 Transient EM/circuit co-simulation.

modeling biological tissues, both thermal solvers have been extended to include the bio-heat equation.

NEW PRODUCTS

Version 2009 features two entirely new products: CST PCB STUDIO™

(CST PCBS) and CST CABLE STUDIO™ (CST CS). Both are based on SimLab technology and are fully integrated in the CST DESIGN ENVIRONMENT™. CST CS simulates fields on cable harnesses while CST PCBS focuses on PCBs. Signal integrity and conducted emissions can be directly evaluated in these tools, and calculated surface currents can be used to conduct a radiation analysis in CST MWS.

CONCLUSION

Version 2009 efficiently leverages new technologies to reduce simulation times and increase interoperability offering improved usability and simulation capabilities, as well as two new products. As a result users benefit from an accurate and reliable tool that speeds up their design process and smoothly integrates into existing design flows.

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A MICROWAVE CABLE FAMILY WITH ULTRA LOW INSERTION LOSS

In 1983, the SUCOFLEX 100 microwave cable family from HUBER+SUHNER impacted greatly on the market and to this day continues to hold its own as a leading product family. Its extensive product range and electrical and mechanical characteristics, allied to high reliability, has enabled the family to be

widely used worldwide. The new SUCOFLEX 400 cable family has been designed with new features that will enable it to continue the tradition and set new standards for microwave cable assemblies, particularly in the test and measurement, defense, instrumentation and space markets.

NEW REQUIREMENTS

In recent years, the requirements that cable assemblies must meet have changed and become increasingly demanding. For example, vibration,

shock, the need for the lowest phase change in relation to temperature, RF-leakage, moisture and chemical resistance, weight, etc., are of enormous importance in defense technology. In the test and measurement market, requirements such as Flex-Life, small phase change versus bending and torsion, and high loss stability in the case of bending and shaking are priority considerations.

To better meet specific market needs, HUBER+SUHNER initiated a major initiative with the goal of designing future products, each with a market focus—basically providing a tailor-made solution for each target group. The first result of this initiative was the development of the SUCOFLEX 300 family for aerospace applications; the SUCOFLEX 400 is the latest range to be produced.

LOW INSERTION LOSS

The SUCOFLEX 400's construction (shown in **Figure 1**) is a solid silver-plated copper wire center conductor, encased by an extruded ultra low density PTFE dielectric, with a silver-plated copper tape inner shield, a silver-plated copper braid outer shield and a Fluorinated Ethylene Propylene (FEP) jacket.

Of particular significance is the new, extruded ultra low density PTFE dielectric, with a dielectric constant of 1.26, giving the SU-COFLEX 400 the lowest insertion loss

TABLE I

ELECTRICAL CHARACTERISTICS OF THE SUCOFLEX 404

Impedance	50 ± 1 Ω
Operating frequency	26.5 GHz
Diameter	5.5 mm
Capacitance	74.8 pF/m (22.8 pF/ft)
Velocity of propagation	89%
Signal delay	3.74 ns/m (1.14 ns/ft)
Nominal phase	1347°/GHz/m (410.5°/GHz/ft)
Phase stability vs. temperature	See graph 1+2
Insertion loss stability vs. temperature	< 0.0023 /°C
Insertion loss stability vs. bending	< 0.05 dB
Screening effectiveness up to 18 GHz	> 90 dB
Attenuation	See table 1
CW power	See table 1
Return loss with straight SMA connectors	Min. 20.0 dB up to 18.0 GHz

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Herisau, Switzerland

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High Rel is our forte; we service some of the most prestigious connector/filter houses in the nation, providing them with the highest standards in quality and customer service. We pride ourselves in knowing that many orbital and communications satellites contain parts plated at our facility.

Typical Applications



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Attenuators	Connectors	EMI Shielding
Waveguides	Contacts	Kovar Carriers
Masking Available		PC Board Hardware

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currently available. And, despite the proportion of air, the proven mechanical stability and reliability of the extruded dielectric has been preserved. The cable's electrical characteristics are shown in **Table 1**.

Another highlight of the very low dielectric constant is that the Continuous Wave (CW) power capability has been increased together with a very significant improvement in phase stability versus temperature (shown in **Figures 2a** and **2b**). This is a great advantage in applications such as phased-array antenna systems and also helps to simplify the adjustment of radars. The attenuation/CW power is shown in **Table 2**.

The new family of microwave cables has been specifically developed for applications on the ground for defense technology, medical and space measurement technology applications, where the lowest loss, highest performance, best phase stability versus temperature and phase stability versus bending, good return loss and mechanical stability are of the utmost importance.

DIVERSE APPLICATIONS

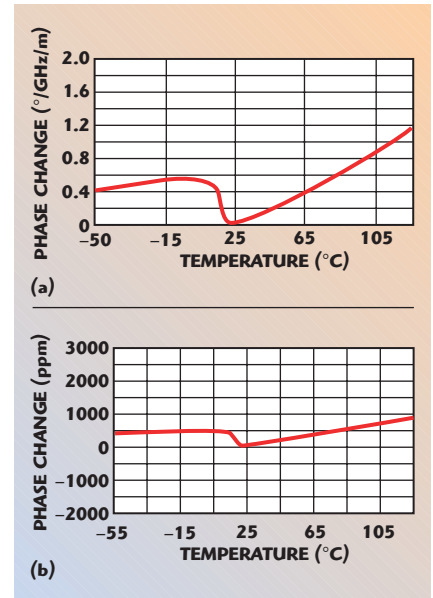
The new microwave cable assembly is suitable for different applications. In defense technology, its primary use is in tactical and strategic communications and in electronic warfare (radar systems, etc.). In particular, phase-matched cable assemblies are required for radar applications. Complete sets of phase-matched, time-delay-matched or amplitude-matched SUCOFLEX 400 cable assemblies are available.

The special characteristics of the new cable assembly family are also likely to make it the preferred solution for thermal vacuum tests for satellite components or for entire satellites, as well as for applications in medical systems such as high frequency ablations of cancerous ulcers or connections between high frequency generators and probes.

The cable assemblies have been tested in accordance with the relevant MIL specifications and standards and, as a result, are suitable for numerous applications in defense technology. The



▲ Fig. 1 A graphical illustration of the construction of the SUCOFLEX 400.



▲ Fig. 2 Phase stability vs. temperature (°/GHz/m vs. °C) (a); phase stability vs. temperature (ppm vs. °C) (b).

MISSION POSSIBLE



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Ultra-Low Phase Noise

(-143 dBc/Hz @ 100 kHz)

& Fine Frequency Resolution

(Fpd less than 1 kHz)

products will also be subjected to a special TVAC test program for thermal vacuum applications.

PRODUCT LAUNCH

There will be a steady roll-out of SUCOFLEX 400 products for specific relevant markets starting with the SUCOFLEX 404 (diameter 5.5 mm) with a straight male SMA connector, which will be available this month (October 2008). The SUCOFLEX 406 (diameter 7.9 mm) including N and TNC straight male connectors will follow at the beginning of 2009. This cable will have the lowest loss of the family and thus be the lowest loss product up to 18 GHz on the market. During the course of 2009, the connector range will be expanded and followed by additional thinner versions with the lowest losses for frequencies up to 40 GHz, as well as additional jackets and armor for all kinds of applications.

CONCLUSION

The SUCOFLEX 400 family of microwave cable assemblies is identical in design with the familiar SUCOFLEX 100 products, which have proven their reliability and stability for a wide range of applications for more than 20 years. The latest innovation though, is the new ultra low density PTFE dielectric, which has been completely redesigned and, as a result, has improved the electrical performance of the new cable. The connectors, likewise developed by HUBER+SUHNER, have been adjusted to the cable in order to preserve the excellent return loss (VSWR) on the assembly.

TABLE II

ATTENUATION/CW POWER

Frequency (GHz)	Attenuation (dB/m)	Attenuation (dB/ft)	CW Power (W) sea level, 40 °C
2.0	0.30	0.09	689
4.0	0.42	0.13	488
6.0	0.52	0.16	398
8.0	0.61	0.19	345
10.0	0.68	0.21	308
12.0	0.75	0.23	281
14.0	0.82	0.25	260
16.0	0.88	0.27	243
18.0	0.95	0.29	230
26.5	1.15	0.35	189

Current HF systems for defense, medical and space applications must comply with the highest demands, so it is essential that the accompanying connection components meet the highest standards too. The new SUCOFLEX 400 family meets these demands.

**HUBER+SUHNER AG, Herisau, Switzerland,
+41 71 353 41 11, www.hubersuhner.com.**

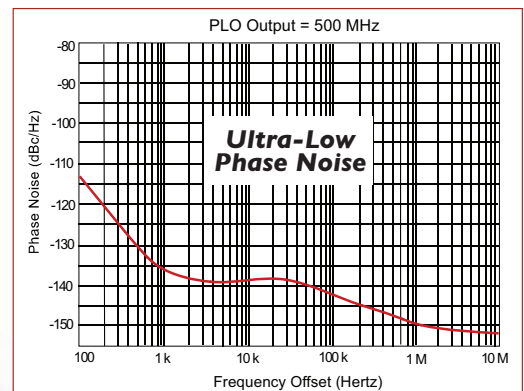
RS No. 301

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Capabilities Brochure

Learn about all capabilities of Aeroflex IQCreator™ software in this new product brochure. Designed for use with Aeroflex's digital RF signal generators, including the 3410 and PXI-based 3000 Series, IQCreator enables you to create waveforms that emulate digitally modulated RF and analog baseband I and Q transmission formats. IQCreator is an easy to use, Windows™-based software application that enables a user to set up a modulation scheme and then create an Arbitrary Waveform Generator (ARB) file.

Aeroflex,
Plainview, NY (800) 835-2350, www.aeroflex.com.

RS No. 310

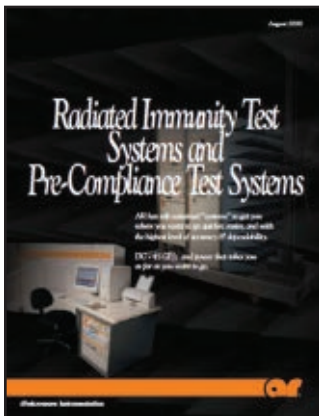


Switch Selection Guide

Agilent's new "RF and Microwave Switch Selection Guide" provides comprehensive information on the company's entire portfolio of switches. The guide provides an overview of electromechanical and solid-state switches and switch drivers. Characteristic switch parameters such as switching speed, isolation and insertion loss including typical applications and configuration are provided. To download a free copy, visit www.agilent.com/find/switches.

Agilent Technologies,
Santa Clara, CA (800) 829-4444, www.agilent.com.

RS No. 311



AR Systems Brochure

AR RF/Microwave Instrumentation's newest brochure highlights its systems' capabilities and AR-Cell Precompliance Test Systems. AR has the capabilities to customize systems to solve your RF and EMC test problems with the power and frequency you need – from 10 kHz to 45 GHz. The AR-Cell systems are out-of-the-box immunity and emissions test systems that perform precompliance testing to IEC 61000-4-3 requirements as well as other industry specific standards.

AR RF/Microwave Instrumentation,
Souderton, PA (215) 723-8181, www.ar-worldwide.com.

RS No. 312



Enhanced Catalog

With 62 pages the new 2008 AtlantecRF catalog is bigger than ever. It features many new additions to the product ranges, most notably: synthesized local oscillators, a new phase-locked oscillator with internal TCXO reference (APL-04), mixers, terminations, medium power attenuators, filters, PIN switches and cable assemblies. The catalog offers detailed specifications for each product, including dimensional diagrams, etc. It also contains information on the ranges of custom equipment and components.

AtlantecRF,
Braintree, Essex, UK +44 1376 550220, www.atlantecrf.com.

RS No. 313



Product Catalog

This 36-page catalog features 175 all-new amplifier products, including lightweight and compact LNAs based on GaAs PHEMT active devices. CTT's extended product offering includes Gallium Nitride (GaN)-based power amplifiers for wideband jammer applications (25 W from 0.5 to 2.0 GHz), as well as narrowband radar applications (80 W from 8.5 to 9.6 GHz). In addition, several new subsystem offerings have been introduced including a VMEbus-compatible two-channel IF conditioner.

CTT Inc.,
Sunnyvale, CA (408) 541-0596, www.cttinc.com.

RS No. 314



Interactive Product Catalog

This web site provides a comprehensive, user-friendly selection of the company's products and functionality to configure and submit quote requests. The site features a parametric search engine and a collection of RF engineer's applets such as a watts-to-dBm converter, gain calculator and links to contact

Empower's sales team. There is also a mobile-friendly version accessible from devices such as a RIM Blackberry. The mobile site has a product selector, contact information and driving directions from Los Angeles Airport.

Empower RF Systems Inc.,
Inglewood, CA (310) 412-8100, www.empowerrf.com.

RS No. 315

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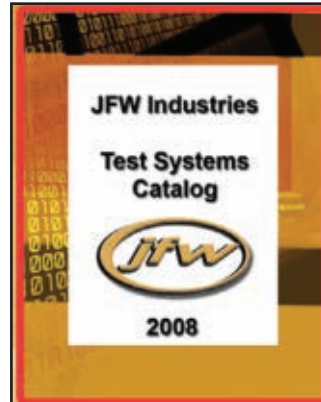


RF Systems and Components

The new 2008 product folder from eubus GmbH combines all detailed data sheets of the RF systems and RF components product portfolio. The RF systems part contains all network attenuator module (NAM) products and the handover and coupling unit (HCU). The RF components part shows all power dividers/combiners, solid-state programmable attenuators, RF switch modules as well as directional couplers.

eubus GmbH,
München, Germany +49 (0) 89 4522 578 11, www.eubus.net.

RS No. 316

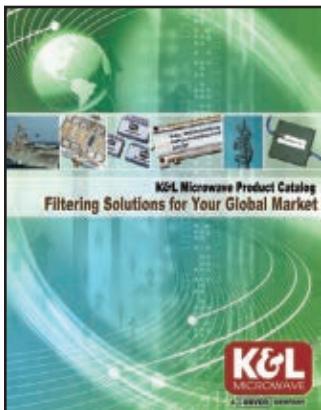


Test Systems Catalog

This test systems catalog features programmable attenuator assemblies, handover test systems, transceiver test systems, switch assemblies, matrix switches, Ethernet, RS-232 and GPIB command information. To download the catalog or request a printed catalog, visit www.jfwindustries.com.

JFW Industries Inc.,
Indianapolis, IN (317) 887-1340, www.jfwindustries.com.

RS No. 317

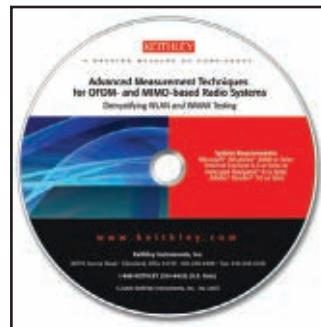


RF and Microwave Filter Catalog

K&L Microwave's new catalog features RF and microwave filter products that are essential for defense electronics and telecommunication systems. Integrated assemblies and a wide assortment of lumped component, cavity, ceramic and suspended substrate filters are among the many types of products included in this 128-page catalog.

K&L Microwave,
Salisbury, MD (410) 749-2424, www.klmicrowave.com;
www.klfilterwizard.com.

RS No. 318



Wireless and RF Testing Guide

Advanced Measurement Techniques for OFDM- and MIMO-based Radio Systems: Demystifying WLAN and WiMAX Testing gives test engineers a broad range of information on the fast changing wireless communication and RF testing field for a wide array of applications, including spectrum analyzer power averaging, as well as the most challenging testing of

the most complex signals, such as OFDM, MIMO and WiMAX. This CD contains useful and informative RF testing resources, including application notes, articles and white papers.

Keithley Instruments Inc.,
Cleveland, OH (440) 248-0400, www.keithley.com.

RS No. 319



Selection Guide

The electromechanical relays selection guide has been modified into an easy-to-use guide for engineers to quickly choose a product through a comprehensive part number development tool for each relay family. The new 24-page EMR selection guide features RF, commercial, military, special environment and Teledyne's Established Reliability relays. Screening levels for the Military and Established Reliability relays are also included.

Teledyne Relays,
Thousand Oaks, CA (805) 373-4545, www.teledynereleys.com.

RS No. 320




Product Brochure

This brochure provides a brief, descriptive overview of the LMR® family of cables and connectors, including the acclaimed Advantage™ series. The brochure also includes T-RAD® leaky feeder cable for interior coverage solutions, SilverLine™ test cables including SilverLine QMA and SilverLine TuffGrip™ and also TCOM® flexible low-PIM cables. LMR cables are flexible, non-kinking low loss RF transmission line cables that utilize easy-to-install connectors.

Times Microwave Systems,
Wallingford, CT (203) 949-8400, www.timesmicrowave.com.

RS No. 321



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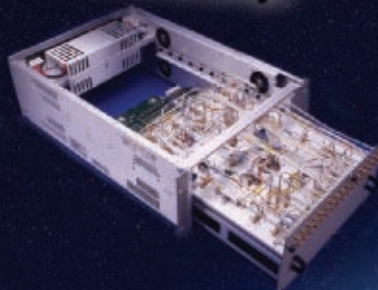
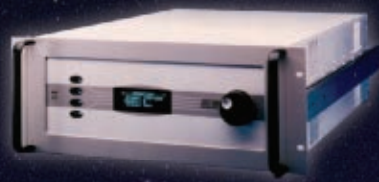
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CATALOG UPDATE



Product Catalog

Valpey Fisher Corp. specializes in low noise timing solutions. From discrete high precision crystal oscillators to highly integrated low noise timing modules, Valpey Fisher offers a broad array of frequency control products needed in advanced timing applications including wireless and wireline infra-

structure, avionics, test and measurement, and military communications. The product catalog is filled with the latest innovative timing and frequency control products. Visit the company's web site for a digital copy of the catalog. Products include: timing modules, OCXOs, TCXOs, VCXOs, XO's and hi-rel COTS.

Valpey Fisher Corp.,
Hopkinton, MA (800) 982-5737, www.valpeyfisher.com.

RS No. 322



Product Catalog

Weinschel Associates, a manufacturer of high-quality broadband RF and microwave products for commercial and military markets both domestic and international, has just released the 2009 edition of its full-line catalog. The company's goal is to serve you, the customer, with an ever increasing usefulness of product line.

Weinschel Associates,
Gaithersburg, MD (301) 963-4630,
www.weinschelassociates.com.

RS No. 323



Product Guide

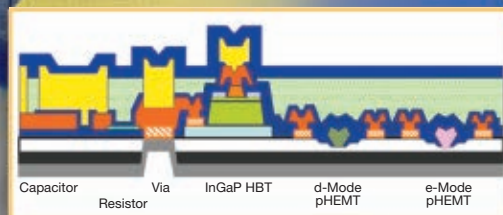
Z-Communications Inc. announced the release of the company's 2008 product guide. This short form catalog includes a wide variety of surface-mount voltage-controlled oscillator (VCO) and phase-locked loop (PLL) synthesizer modules ranging from 40 MHz to 10 GHz. In addition to high performance parts and specifications, the guide features detailed outline drawings, footprints and test fixtures. Users can download an electronic version of the product guide on-line at www.zcomm.com or contact the

company at sales@zcomm.com for a hard copy version.

Z-Communications Inc.,
San Diego, CA (858) 621-2700, www.zcomm.com.

RS No. 324

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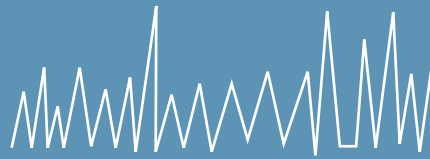
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■ High Power GaN Amplifier

The model SSPA 3.1-3.5-1300-RM is a high power, pulsed RF amplifier that operates from 3.1 to 3.5 GHz in a rack-mounted configuration. This PA is ideal for

S-band military radars. It is packaged in a 3U high, 19 inch rack-mounted enclosure. This amplifier has a minimum peak output power of 1300 W at a 5 percent duty cycle with a 64 uSec pulse width. This amplifier offers a typical saturated gain of 38 dB with a typical power flatness of ± 1.0 dB with an input drive of 24 dBm ± 1.0 dB. Input and output VSWR is 1.5 maximum. This RF rack-mounted amplifier operates from 208 to 220 VAC. There is a forward power RF sample port along with an output forward detected voltage pulse available.

Aethercomm Inc., San Marcos, CA
(760) 598-4340, www.aethercomm.com.

RS No. 249

■ Low Noise Synthesizers

The ESP-1100 and ESP-1700 were designed for use as local oscillators in converters for fading channel simulators, operating at fixed-frequencies (1100 MHz and 1700 MHz), with extremely low phase noise of < -143 dBc/Hz at 100 kHz and < -138 dBc/Hz at 100 kHz, respectively. The ESP series features output powers up to +14 dBm, external or internal frequency references, in a small connectorized package, 2.25" x 2.25" x 0.6". Originally configured for laboratory and ground-based applications, this part is extremely robust, will handle high levels of shock and vibration, and can be hermetically-sealed for use in high-rel military applications.

EM Research Inc., Reno, NV
(775) 345-2411, www.emresearch.com.

RS No. 216

■ Active x2 Multiplier

The HMC598 active x2 frequency multiplier utilizes GaAs PHEMT technology, and is offered in bare die form. The device is comprised of an input amplifier, a low conversion loss frequency doubler, and an output buffer amplifier. When driven with a +5 dBm input signal, this frequency multiplier provides +15 dBm typical output power from 22 to 46 GHz, and the Fo and 3Fo isolations are 25 dBc and 15 dBc respectively at 30 GHz. This multiplier is ideal for clock generation, microwave radio and test equipment applications.

Hittite Microwave Corp., Chelmsford, MA
(978) 250-3343, www.hittite.com.

RS No. 217

■ TWT Amplifier

The model 8923H is a dual-band 300 W 30 GHz/175 W 45 GHz Traveling Wave Tube (TWT) amplifier. Designed for military SATCOM uplink applications, this TWT has a remarkably small

footprint and weighs less than four pounds. L-3 ETI's model 8923H TWT operates in a frequency range from 30 to 45.5 GHz, including the 33 to 36 GHz radar band, and incorporates focus electrode modulation to allow both CW and pulsed operation. This product introduction complements L-3 ETI's existing 8926HB 500 W Ka-band TWT (27.5 to 31 GHz) and 8925HP 200 W Q-band TWT (43.5 to 45.5 GHz).

L-3 Electron Technologies Inc., Torrance, CA (310) 517-6000,
www.l-3com.com.

RS No. 218

■ High Power Limiter

The model CCS33060 is a high power, self-biased limiter that operates from 10 MHz to 18 GHz. The input power specification is 180 W CW, 600 W peak. The flat leakage is 17 dBm maximum,

and the insertion loss is 0.8 dB maximum. This device has a VSWR of 1.35 maximum and a recovery time of 5 uSec maximum. The input connector is a JGMS and the output connector is a removable SMA. This device uses a self-biased PIN/Schottky input stage with a PIN clean-up stage.

Cobham Defense Electronic Systems, REMEC Defense and Space East, Manchester, NH (603) 518-2700,
www.remecrds.com.

RS No. 219

■ 4 W Linear Power Amplifier

The model SM06927-36H is a 690 to 2700 MHz solid-state GaAs FET amplifier designed

for multi-purpose use in multiple wireless and military markets. This module provides a minimum of +36 dBm of output

power at P1dB with an OIP3 of +48 dBm. The gain flatness over the entire 2.1 GHz bandwidth is ± 0.75 dB. The unit uses the latest surface-mount technologies to provide numerous features, while maintaining a minimal size. Price: \$1200 (1-3). Delivery: three to four weeks.

Stealth Microwave Inc., Trenton, NJ
(609) 538-8586,
www.stealthmicrowave.com.

RS No. 220

■ VME-based Receiver

The model SYS1000N01U is a VME-based receiver that features a multi-stage superhetrodyne architecture design. The design will translate an X-band signal with the frequency excursion of 1,000

MHz to an IF center frequency of 70 MHz with an instantaneous bandwidth of 20 MHz. The receiver functionality includes automatic gain control (AGC) attenuator with analog sampling, channel gain balance attenuator, channel phase balance phase shifter, signal injection point, peak detected signals (available via VME interface) and RF signal monitoring points. The receiver is fabricated into a three-slot wide VME module. Control of the receiver components is done using standard VME-64 bus protocol.

MITEQ Inc., Hauppauge, NY
(631) 436-7400, www.miteq.com.

RS No. 242

■ Monitoring Receiver

The model RMR-818-77-NRL is an 8 to 18 GHz radar/microwave monitoring receiver for laboratory applications. The receiver uses an extended range detector log video amplifier (DLVA), a pre-

amplifier and RF bandpass filtering. It also offers a dynamic range of 75 dB with a typical TSS of -80 dBm. It can be supplied with either individually removable bandpass filters or various switched filter bank options. The basic model offers a log video output for analysis through external test equipment. These microwave monitoring receivers are available in frequency ranges from 0.5 to 20 GHz as well as different sizes and capabilities.

Planar Monolithics Industries Inc., Frederick, MD (301) 631-1579,
www.planarmonolithics.com.

RS No. 243

■ Calibrated Noise Source

The NW-CS-I series is a high level calibrated noise source equipped with an internal isolator allowing high output noise to be generated with an excellent VSWR. Standard output levels are 30 to 35 dB ENR with units as high as 40 dB available. These units are ideal for built-in test application in early warning radar systems and satellite test systems to calibrate receivers. Due to their high output levels they can be injected via couplers and into high loss networks. The unit is integrated into a small package saving space.

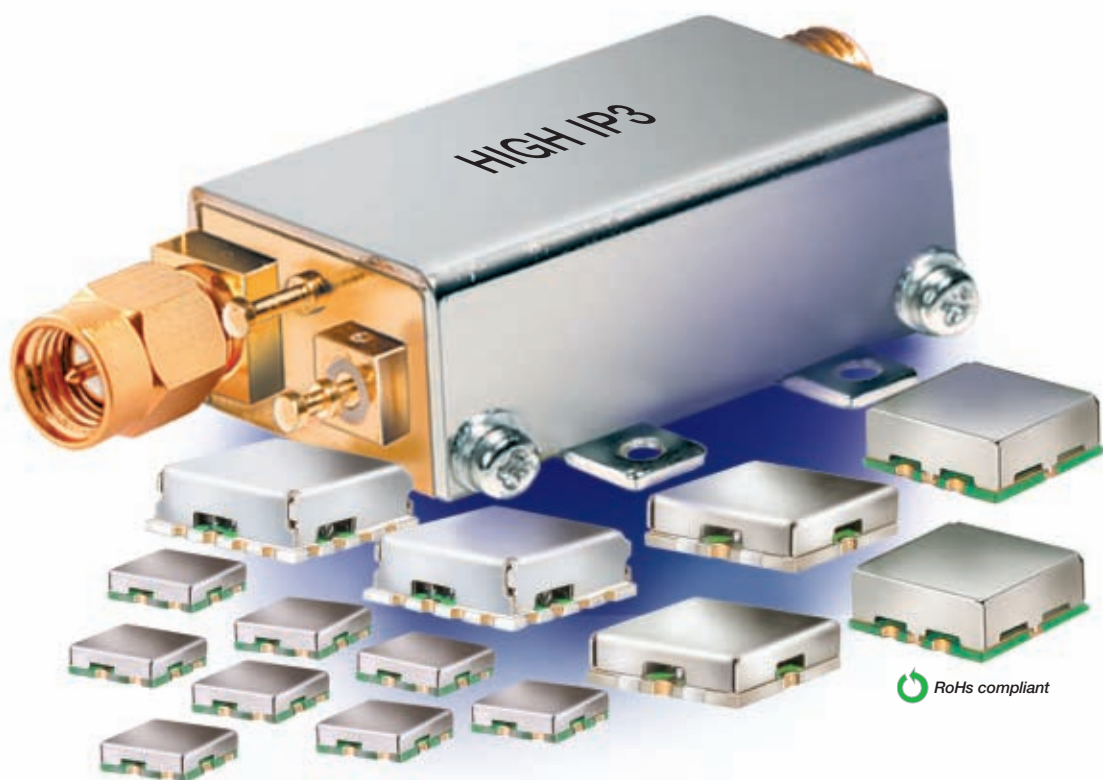
NoiseWave, East Hanover, NJ
(973) 386-1119, www.noisewave.com.

RS No. 246

Constant Impedance

VVAs

10 to 3000 MHz



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Voltage Variable Attenuators (VVAs) deliver as high as 40 dB attenuation control over the 10 MHz through 3.0 GHz range. Offered in both 50 and 75 Ω models these surface-mount and coaxial low-cost VVAs require no external components and maintain a good impedance match over the entire frequency and attenuation range, typically 20 dB return loss at input and output ports. These high performance units offer insertion loss as low as 1.5 dB, typical IP3 performance as high as +56 dBm, and minimal phase variation low as 7°.

Mini-Circuits VVAs are enclosed in shielded surface-mount cases as small as 0.3" x 0.3" x 0.1". Coaxial models are available with unibody case with SMA connectors. Applications include automatic-level-control (ALC) circuits, gain and power level control, and leveling in feedforward amplifiers. Visit the Mini-Circuits website at www.minicircuits.com for comprehensive performance data, circuit layouts, environmental specifications and real-time price and availability.

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Active Components

Temperature-compensated Crystal Oscillator

The model VFTX312 is a temperature-compensated crystal oscillator (TCXO) with a voltage control option suitable for FEMTO CELL reference timing. The output frequency of 26 MHz and the tight temperature stability of

0.1 ppm is specifically designed for 3GPP (Femto Cell) system timing. This TCXO is a fundamental mode crystal oscillator with low power consumption. Available in a 5x7 mm surface-mount hermetically-sealed package that is fully RoHS 6/6 compliant.

Valpey Fisher Corp., Hopkinton, MA
(508) 435-6831, www.valpeyfisher.com.

RS No. 221

Low Phase Noise Frequency Multiplier

The Holzworth HX4110 frequency multiplier is a laboratory grade reference multiplier that can be used for any 10 to 100 MHz conversion. The HX4110 has a unique circuit architecture that maintains the low phase noise and low jitter characteristics of precision oscillators and RF



sources. With typical additive phase noise performance of -174 dBc/Hz (input referred), the HX4110 is an excellent choice for sensitive laboratory applications as well as high performance transmitter/receiver applications. Holzworth products are 100 percent final performance tested for phase noise verification.

Holzworth Instrumentation, Boulder, CO
(303) 325-3473, www.holzworth.com.

RS No. 222

Voltage-controlled Oscillators

These economical voltage-controlled oscillators (VCO) offer low phase noise in the industry-standard one half inch square package. Model MD111MST operates in a frequency range from 950 to 980 MHz and is rated -119 dBc at

10 kHz offset. Many other catalog models are available and custom designs can be supplied with no NRE.

Modco Inc., Sparks, NV (775) 331-2442,
www.modcoinc.com.

RS No. 223

Micro-miniature SMA Switch

This micro-miniature SMA switch is a single-pole two position type. The switch incorporates

sources. With typical additive phase noise performance of -174 dBc/Hz (input referred), the HX4110 is



SMA connectors to allow high density packaging and excellent electrical performance through 26.5 GHz. The switch is available

in failsafe and latching configurations with a choice of three different frequency ranges and three different coil voltages.

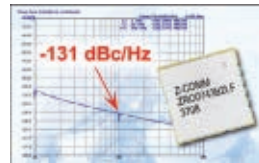
RLC Electronics Inc., Mount Kisco, NY
(914) 241-1334, www.rlcelectronics.com.

RS No. 224

Voltage-controlled Oscillator

The model ZRO0743B2LF is a coaxial resonator based voltage-controlled oscillator (VCO) that operates in a frequency range from 738 to 748 MHz with a tuning voltage range of 0 to 6 VDC. This VCO features an excellent

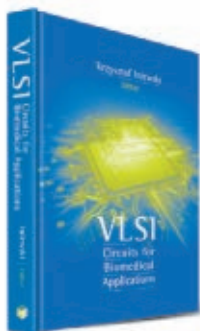
typical phase noise of -131 dBc/Hz at 10 kHz offset and a typical tuning sensitivity of 2 MHz/V. The ZRO0743B2LF is designed to deliver a typical output power of 9 dBm at 8 VDC supply while drawing 23 mA (typical) over the temperature range of -40° to 85°C. The ZRO0743B2LF has a typical phase noise value of -104 dBc/Hz at 1 kHz offset and -151 dBc/Hz at 100 kHz offset. This VCO features typical second harmonic suppression of -20 dBc and comes in Z-COMM's newly developed



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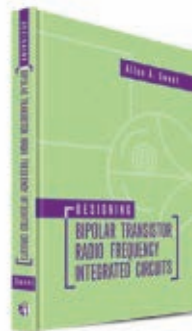
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RS No. 226

Amplifier

Low Noise Amplifiers

The model ZX60-0916LN+ is an ultra-low noise amplifier that boasts a noise figure of only 0.55 dB, while delivering 18 dB gain and a high output power of up to 16.5 dBm. Ultra reliable and packaged in a



rugged patented unibody housing, using SMA connectors, these amplifiers provide for a broad range of applications from 824 to 960 MHz, including: CDMA: 824 to 894 MHz, GSM Rx: 880 to 915 MHz and GSM Tx: 925 to 960 MHz. Price: \$39.95 (1-9). Delivery: available from stock.

Mini-Circuits, Brooklyn, NY (718) 934-4500, www.minicircuits.com.

RS No. 227

Antenna

WLAN Antenna

The model HRP2-54-N antenna is a 2' (0.6 m) diameter high performance single linear polar-

ized design and operates in the 4.94 to 4.99 GHz public safety band and the unlicensed frequency bands of 5.25 to 5.85 GHz. Antenna



gain is 26.7 to 28.5 dBi. HPBW's are 7.0 to 6.2 degrees. VSWR is 1.5 maximum. F/B is 43 dB or better. RF input is type N female. The antenna offers manual polarization adjustment for vertical and horizontal polarization settings. The antenna incorporates a sturdy aluminum parabolic main reflector and aluminum shroud with a UV stabilized planar radome.

mWAVE Industries LLC, Windham, ME (207) 892-0011, www.mwavellc.com.

RS No. 229

Passive Components

In-phase Splitter



The model SPD-90-210 is an L-band, four-way in-phase splitter for SATCOM applications. This low loss splitter spans the frequency band of

900 to 2100 MHz while maintaining tight phase and amplitude tracking, typically within 3 degrees and 0.2 dB of signal unbalances respectively within specified frequency band. This product replac-

es stripline splitters and saves critical board space when splitting local oscillator signals and when used as receiver antenna combiners. Size: 0.8" x 0.4" x 0.2". Prices start at \$20.00 for low quantities, with deliveries ranging from stock to six weeks.

Synergy Microwave Corp., Paterson, NJ (973) 881-8800, www.synergymicrowave.com.

RS No. 225

Phase Invariant Attenuator

The model APD3-0080G-0180G-111A is an 8 to 18 GHz phase invariant digital program-



mable attenuator. A double-balanced arrangement of quadrature couplers and PIN diodes gives phase invariant attenuation. It has an attenuation range of

32 dB, insertion loss of < 5.5 dB and VSWR of 2.0. This model offers attenuation accuracy of ± 0.5 dB, flatness of ± 0.8 dB from 0 to 20 dB and ± 1.0 dB from 20 to 32 dB. Switching speed is < 350 ns. Size: 2.5" x 2" x 0.5".

American Microwave Corp., Frederick, MD (301) 662-4702, www.americanmicrowavecorp.com.

RS No. 230

Low Pass Filters

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GA0830-4344-M	0.8~3.0	25W(min)
GA0830-4344-R	0.8~3.0	25W(min)
GA0830-4747-M	0.8~3.0	50W(min)
GA0830-4747-R	0.8~3.0	50W(min)
GA0827-4552-M	0.8~2.7	150W(min)
GA0827-4552-R	0.8~2.7	150W(min)
GA0827-4754-R	0.8~2.7	250W(min)
CON0827-150W-R	0.8~2.7	150W Peak

* Suffix "-M" is Module type, "-R" is Rack type.



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many spectral purity problems. These suspended substrate filters, which are available with standard cut-off frequencies from 1 to 18 GHz, can be quickly installed in



communications equipment according to operating needs and as 'select-on-test' components prior to commissioning. The quasi-elliptical function provides typical insertion loss in the passband of 1.2 dB with stopband attenuation in excess of 50 dB and power handling of 15 W CW.

AtlanTecRF, Braintree, UK

+44 1376 550220, www.atlantecrf.com.

RS No. 231

WiFi/WiMAX Power Dividers

The model 151-173-002 is a two-way, 50 Ω , DC to 6 GHz, 1 W unit with SMA female connectors. Insertion loss is ± 0.5 dB maximum DC to 4 GHz and ± 0.8 dB maximum 4 to 6 GHz with maximum VSWR 1.50. Model 151-231-004 is a four-way, 50 Ω , DC to 6 GHz, 5 W unit with SMA female connectors. Insertion loss is ± 1.0 dB nominal with maximum VSWR 1.50. These devices are ideal for dividing signals for in-building wireless, WiFi, WiMAX and Homeland Security/Public Safety systems.

BroadWave Technologies Inc., Franklin, IN
(317) 346-6101, www.broadwavetech.com.

RS No. 232

High Power Band Reject Filter

The model WSN-00198 is a high power band reject filter positioned at the output of a VHF-UHF amplifier. The filter attenuates an undesired harmonic by 60 dB, while maintaining low loss passbands utilizing special features to extend the upper passband to 500 MHz.

K&L Microwave, Salisbury, MD

(410) 749-2424, www.klmicrowave.com.

RS No. 233

PCS High Power Cavity Duplexer

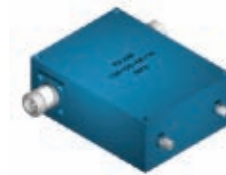
The model WP-D00001 is a duplexer that covers the full Personal Communication System (PCS) frequencies. This duplexer exhibits less than 0.8 dB of insertion loss across the passbands of 1850 to 1910 MHz and 1930 to 1990 MHz while providing greater than 60 dB of rejection. The unit will handle 500 W average power and 10 kW peak power. This unit is designed for mounting on a 3U - 19" rack with a depth of 6.00" and is available from stock.

Lorch Commercial and Wireless, Salisbury, MD (410) 860-5100, www.loorch.com.

RS No. 234

High Power Directional Coupler

The model C50-109-481/1N is a high power directional coupler that operates in a frequency range from 1 to 100 MHz with an insertion loss of 0.2 dB, coupling of 50 ± 1 dB and directivity of 20 dB. The coupling is flat within ± 1.0 dB across the band



and the VSWR is 1.20. Maximum input power is 500 W. Outline dimensions are 3" x 4" x 1.5" and connectors are type N female.

Pulsar Microwave Corp., Clifton, NJ

(973) 779-6262, www.pulsarmicrowave.com.

RS No. 235

RF Coaxial Relay

This newly configured inline five-port 2P2T coaxial relay offers the flexibility of independently operating each of the two sets of switching contacts. The center RF connector port is common to the adjacent output connectors and allows signal path for backup or redundancy mode configuration. Available in 12 and 24 V failsafe with excellent RF performance and power handling capabilities from DC to 18 GHz. Relay measures 2.25" x 0.52" x 1.75". Options include aux contacts, suppression diodes, DC header and logic.

RelComm Technologies Inc., Salisbury, MD (410) 749-4488, www.relcommtech.com.

RS No. 236

Dual Notch Filter

This narrowband dual notch filter attenuates both L1 and L2 GPS frequencies. It is the perfect unit for applications that need to eliminate both of these GPS bands simultaneously, yet can only tolerate a two-port device. A high



power option is available. The company manufactures many different varieties of GPS filters; please contact Reactel with your specific need.

Reactel Inc., Gaithersburg, MD

(301) 519-3660, www.reactel.com.

RS No. 237

6 GHz Fixed Attenuators

This XFP-6 series of 2 W fixed attenuators operates in a frequency range from DC to 6 GHz, with attenuation values from 1 to 40 dB. VSWR is excellent and specified at 1.25 and the attenuation accuracy is typically ± 0.5 dB depending on the dB value. The body and SMA connectors are passivated stainless steel. This series is an ideal solution for test fixtures and signal



leveling applications in UMTS and WiMAX test environments.

Trilithic Inc., Indianapolis, IN
(317) 895-3600, www.trilithic.com.

RS No. 238

■ 30 dB Dual Directional Coupler

The model C3063 is a 30 dB dual directional coupler designed for high power, HF applications. This coupler is rated at 3000 W CW and exhibits exceptional flatness across its entire 0.5 to 32 MHz operating band. Specifications include 0.1 dB insertion loss, 1.05 VSWR, 25 dB directivity and ± 0.25 dB coupling flatness. Size: 6.46" x 2.52" x 1.2".

Werlatone Inc., Brewster, NY
(845) 279-6187, www.werlatone.com.

RS No. 239

Semiconductors/ICs

■ Thermally-enhanced GaN 30 W Devices

Models RT233, RT240 and RT243 are thermally-enhanced gallium nitride devices that offer 36, 43 and 45 dBm measured Psat output power each, from DC to 6 GHz applications. Patent-pending thermally-enhanced technology has been used to improve high temperature reliability and provide added power when used at pulsed applications or Class A amplification. The RT233, RT240 and RT243 transistors are packaged in a thermally-enhanced package, and are available with standard (RT233C, RT240C and RT243C: C-series), or earless type (RT233N, RT240N and RT243N: N-series) designs. Wide-band capable characteristics can give 50 to 2500 MHz wideband applications and other design opportunities.

RFHIC Corp., Suwon, Korea
82-31-250-5011, www.rfhic.com.

RS No. 240

Software

■ IC Package Tool

The VeloceWired™ is a powerful IC package tool that accelerates bondwire design and simulation and enables optimization of high-speed leadframe packages and co-design with analog and mixed-signal ICs. With this tool the bondwire design becomes an integral part of the IC tool flow. It features an efficient and flexible bondwire editor that operates seamlessly in Cadence Virtuoso®. Bondwires are created in 2-D through a simple point-and-click procedure, while their 3-D properties can be edited on-the-fly. Die-to-die and stacked-die configurations are supported.

Helic, Athens, Greece +30 210 9949390,
www.helic.com.

RS No. 241

Test Equipment

■ RF Conducted Immunity Test System



AR RF/Microwave Instrumentation has introduced a new RF conducted immunity test system to test to MIL-STD 461D & E CS114, DO160D & E, EN/IEC 61000-4-6, IEC 60601-1-2,

EN 50130-4, EN 61000-6-1/2 and EN 55024 standards. Model C100400 (10 kHz to 400 MHz) is a fully self-contained unit and includes a signal generator, power meter, 100 W AR amplifier, directional coupler and control software.

AR RF/Microwave Instrumentation, Souderton, PA (215) 723-8181,
www.ar-worldwide.com.

RS No. 244

■ 56 Gb/s Multiplexer and Demultiplexer

The 56 Gb/s 4:1 multiplexer and 56 Gb/s 1:4 demultiplexer is designed to meet current high-speed market needs. The MS4S1V2M is a SiGe 4-to-1 multiplexer designed for use in telecom applications up to 56 Gb/s. The module accepts input data rates from 0.5 to 14 Gb/s with an input sensitivity better than 100 mV. The broad bandwidth of the input allows operation from 2 to 56 Gb/s. The MD1S4V2M is a SiGe 1-to-4 demultiplexer designed for use in 100G applications operating at transmission speeds within the demultiplexer's 2 to 56 Gb/s input rate. The demux has a very broad input rate, and can be used for a wide range of applications from 2 to 56 Gb/s.

Centellax Inc., Santa Rosa, CA
(866) 522-6888, www.centellax.com.

RS No. 250

■ Pre-matching Tuners

The MT902A series of pre-matching tuners operate in a frequency range from 8 to 50 GHz and are highly stable, low loss wafer probe mounts used in on-wafer device characterization applications. By extending a wafer probe away from the tuner body, these mounts create additional clearance for proper probe alignment. The ultra high stability inherent in their design eliminates the possibility of undesired movement during operation.

Maury Microwave Corp., Ontario, CA
(909) 987-4715, www.maurymic.com.

RS No. 245

■ Microwave Signal Generator Upgrades

The capabilities of the R&S SMF100A microwave signal generator has been expanded with two new options. The R&S SMF-K27 option allows users to configure pulse trains for radar specific devel-



RF Power Amplifiers ALM Series

Low Cost GaAs FET Amplifiers



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ALM00110-2840FM-SMA(F)	10 ~ 1000	10W(min)
ALM1015-2840FM-SMA(F)	1000 ~ 1500	10W(min)
ALM1520-2840FM-SMA(F)	1500 ~ 2000	10W(min)
ALM1922-2840FM-SMA(F)	1900 ~ 2200	15W(min)
ALM00505-4546-SMA	50 ~ 500	40W(min)
ALM0105-4748-SMA	100 ~ 500	60W(min)
ALM0510-3846-SMA	500 ~ 1000	25W(min)
ALM2527-4547-SMA	2500 ~ 2700	50W(min)

* A bench top type is also available that features 100-240V AC.



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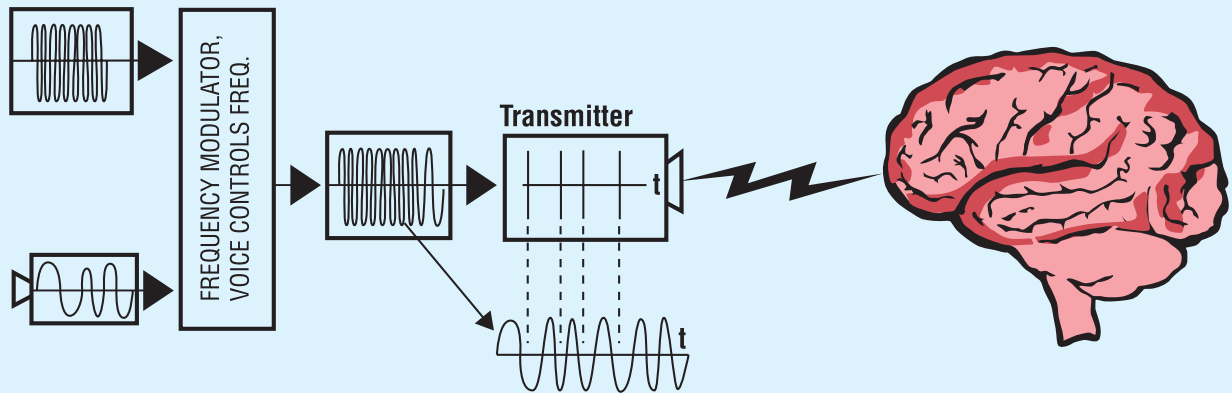
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(727) 344-6254, www.mcli.com.

RS No. 248



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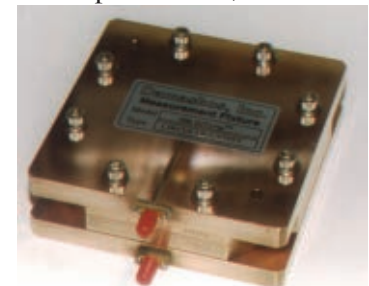
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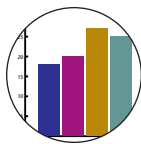
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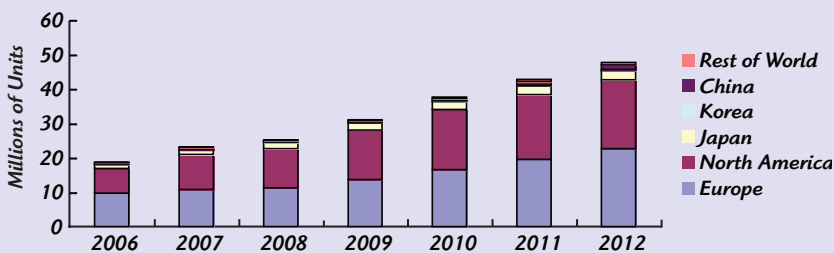


MICROWAVE METRICS

MANDATES RESHAPE MARKET FOR AUTOMOTIVE ELECTRONIC STABILITY CONTROL SYSTEMS

Driven by new government mandates, global market revenue for Micro-electromechanical System (MEMS) sensors used for automotive Electronic Stability Control (ESC) is set to nearly double from 2006 to 2012, according to iSuppli Corp. Worldwide revenue for MEMS ESC sensors will rise to \$715 M in 2012, up from \$378 M in 2006. Global shipments of complete ESC systems are expected to rise to 47.7 million units in 2012, up from 23.1 million in 2007.

Shipments of ESC Systems by Global Region
2006-2012 (Millions of Units)



Source: iSuppli Corp.,

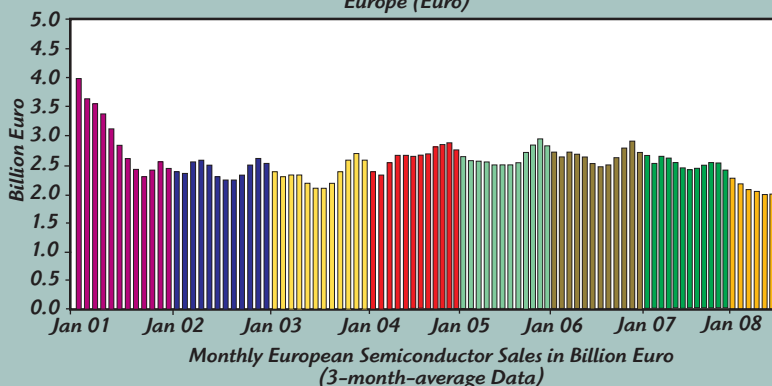
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EUROPEAN SEMICONDUCTOR MARKET

Worldwide sales of semiconductors of \$21.6 B in June were 8% higher than the \$20.0 B reported for June 2007, the World Semiconductor Trade Statistics (WSTS) reports. A flat growth rate can be observed if June sales are compared with the \$21.5 B reported for May 2008. Year-to-date (YTD) sales of \$127.5 B are 5.4% higher than in the first half of the year 2007 when sales were \$121 B.

On the basis of the same comparison, the figures also show that the performance of the European semiconductor market followed a similar positive trend to the world market with a growth rate of 5.1%. Looking at product categories, strong growth was observed for Optoelectronics (31.7%) mainly for industrial, automotive and mobile phones applications, Micro Processing Unit (MPU) (13.2%) for PCs and notebooks but also special purpose ICs for industrial (28.5%), communication (15%) and automotive (9.9%) applications. More in detail, European semiconductor sales in June 2008 amounted to \$3.369 B according to WSTS, up 1.2% versus the previous month. This corresponds to an increase of 5.1% compared to the same month last year. On a YTD basis semiconductor sales increased by 1.9% versus the same period in the year 2007.

Europe (Euro)



Source: European Electronic Component Manufacturers Association,
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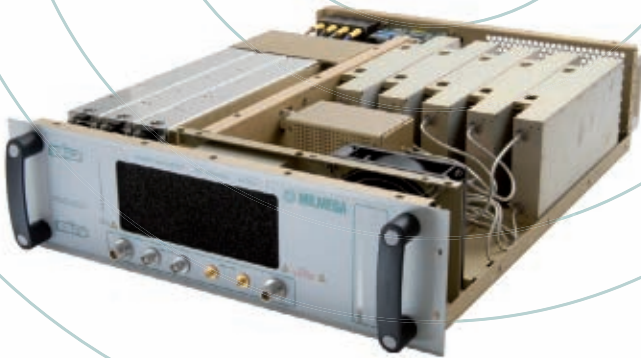
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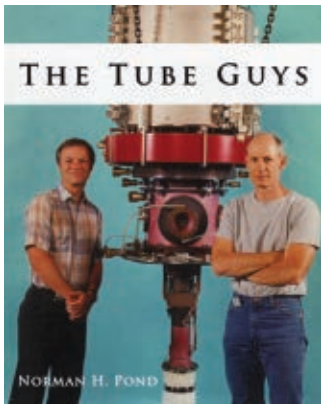
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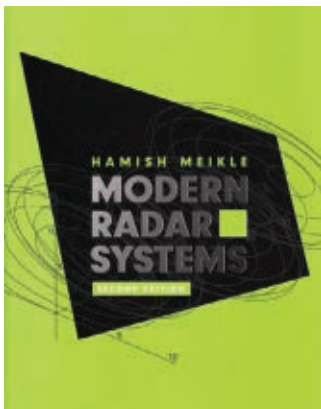
Microwave tubes, a largely unrecognized technology invented at the onset of World War II, have changed the world. Magnetrons and klystrons made radar practical, giving the Allies great advantages in detecting and targeting enemy aircraft. Over the past 70 years, a small group of dedicated people have made continued improvements to this technology and the resulting products affect many aspects of our lives. The purpose of the book is to record its remarkable story and to answer the questions: How did the inventions occur? Who did it? Who were these guys? How did businesses develop? Why did some companies fall by the way side while others flourished? And finally, what does the future hold for this technology? The first chapter traces the roots of the tube industry to Edison light bulb and the first attempts to develop a radio tube by Fleming in the UK and de Forest in the US. The next four chapters are dedicated to the

invention and development of magnetrons and klystrons, which were of such importance during World War II. Then, the inventions of other tubes, such as the travelling tube, the backward wave tube, the Ubitron and Gyrotron are described in four chapters. Two chapters describe the state of the tube industry from the end of World War II to 2007. Non-military uses of microwave tubes, such as linear accelerator, broadband communications and microwave ovens are covered in three chapters. The next 26 chapters consider the formation and consolidation of microwave tube companies and the history of 25 different companies, many of which are no longer operating or have been merged with others. In three chapters, the microwave tube activity in Japan, the former USSR and Germany is described. The final chapter considers the future of microwave tube and the concurrence offered by solid-state technology.

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Hamish Meikle

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The second edition of *Modern Radar Systems* is an extensively revised and expanded version of the successful first edition, published in 2001. Chapter 1 presents the fundamentals of radar, including both primary and secondary radar. Chapter 2 introduces the fundamental methods of vector presentation, modulation polyphase signals and noise, and the probability distributions that are used to represent them. The discussion of radar subsystems starts with Chapter 3 on transmitters, where new material has been included on solid-state devices. Chapter 4 on waveguides and transmission lines now includes material on stripline technology and the description of the many types of microwave components has been updated. An expanded Chapter 5 describes antennas, including a discussion and plots of low-side-lobe monopulse patterns. Chapter 6 covers factors outside the radar: propagation, scattering and clutter. Continuing with radar

subsystems, Chapter 7 is dedicated to the receiver, followed by Chapter 8 on matched and matching filters. Chapter 9 covers detectors and Chapter 10 discusses analog to digital conversion. Here, material on the techniques of conversion at intermediate frequency has been added. Signal processing is the subject of Chapter 11. New material includes detailed mathematics of the log-FTC circuit response to clutter and on the operation of range-cell-averaging constant-false-alarm-rate (CFAR) processing. Threshold and detection issues are discussed in Chapter 12, with plots and graphs covering the steady target and the four Swerling models. Chapter 13 covers the determination of position, with equations for the errors for different measuring procedures. A section on the display of position has been added. Chapter 14 discusses radar performance, including the range equation, accuracy, resolution, stability considerations and operation in jamming.

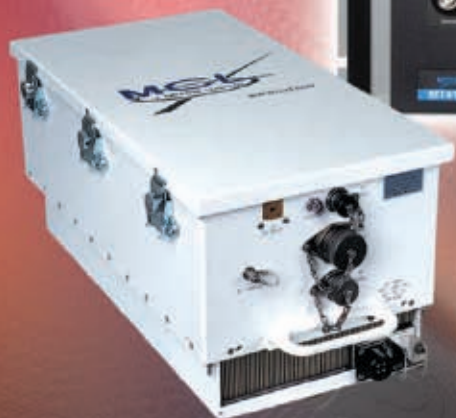
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Branding for RF Engineering Talent

In times when the vacant positions compete on limited RF engineering resources, preparation can help. In here I present the term Branding in the Job Market context as the logical preparation to projected recruiting needs. The more recognized a company is among its technology niche, the more likely it is to gain attention to its recruiting efforts. Branding works here the same way it works in the sales & marketing arena.

RF engineering talent and knowhow (among few other analog fields) is a scarce commodity these days. It is also hard to estimate the cost of an understaffed project. In today's conditions the marketing task imposed on employers and recruiters "selling" their RF engineering positions is not simple. Unlike some other engineering fields, RF engineering projects are typically not tolerant to "on-the-job-training". RF engineering skills are built over many years of hands-on experience. On the other hand, some skill-sets are very hard to come by, and the wait time for the ideal candidate can extend to months and more.

Branding is a way for a company to build recognition among potential customers. Similarly, promoting a company for its technologically challenging career opportunities (in addition to the generic employment appeal factors), increases the attention that later recruiting efforts by that company will receive (e.g. online job postings). Perceived image improves the rate of response to later ads for specific positions. It also encourages RF engineers to make inquiries unrelated to a specific vacancy, serving to build up a database for future use.

People make their career moves for a variety of reasons and the decision process is typically long (months and years). Building recognition in the industry as a viable career alternative, the recruiter captures the attention of those in the midst of that decision process – occasionally before they start their job search. It is a known fact that many of the top-notch engineers never reach the public job market when switching between jobs.

Moreover, this type of promotion in the RF and microwave engineering media reaches customers' engineers and decision makers as well, and hence contributes to the company's sales & marketing efforts.

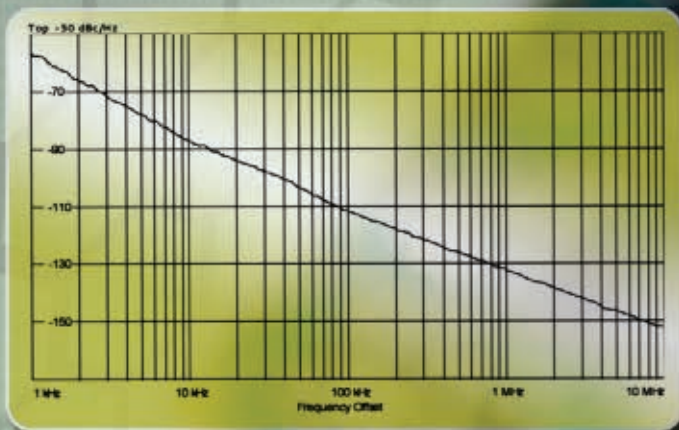
Conclusions: The core industry media channels can be used to highlight and promote a company for its career offerings, reach both engineers and customers. Branding a company as a desired career option in the RF engineering community prepares the cognitive grounds complementing and supporting efforts filling specific RF engineering positions.

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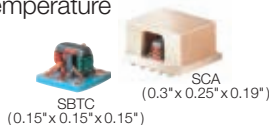
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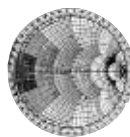
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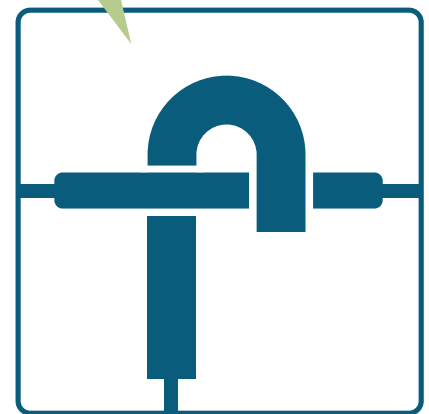
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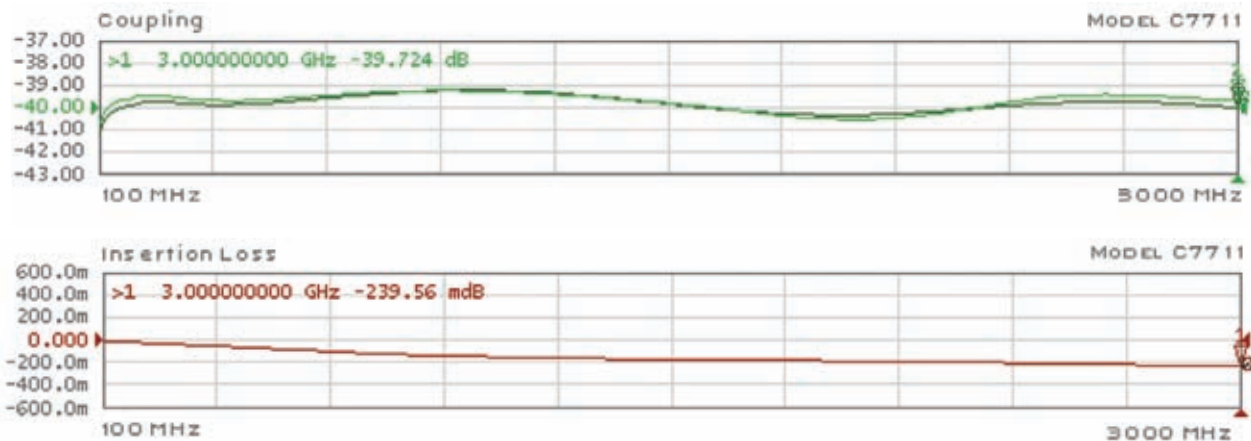


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C7711	Dual Directional	100-3000	100	40	±1.0	0.35	1.25:1	18	3.0 x 2.2 x 0.7
C7783	Bi Directional	200-1000	200	20	±0.75	0.2	1.20:1	20	3.0 x 1.5 x 0.53
C6600	Bi Directional	200-2000	200	20	±1.2	0.25	1.25:1	18	4.0 x 2.0 x 0.72
C7152	Bi Directional	300-3000	100	20	±1.0	0.35	1.20:1	15	3.7 x 2.0 x 0.75
C7811	Dual Directional	500-2500	100	40	±0.5	0.2	1.25:1	20	3.0 x 2.0 x 0.6
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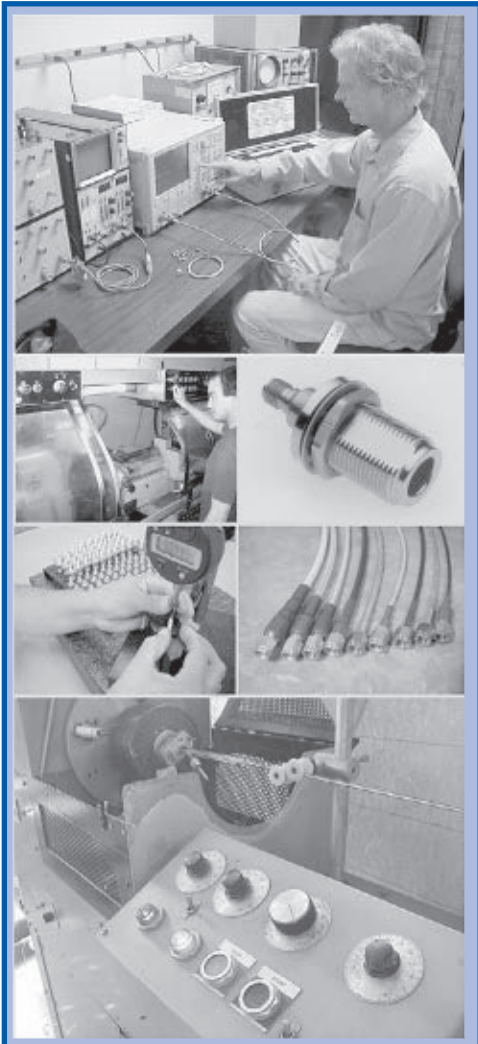
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303-1	8	318-1CC	13	345-CC-PZ	26	355-CC	22	529-2	31	1538-687	40	1579	41
303-1M	8	318-1CC-375	13	345-CC-1 00	11	355-CCFL	22	529-2CLP	31	1538-687 O	40	1587-1	36
303-1 PZ	25	318-2CC	13	345-CC-2	11	356-CC	22	529-3	31	1539	38	1587-2	36
303-2 PZ	25	318-2CC-375	13	345-CC-2H-PZ	26	356-CCFL	22	529-3CLP	31	1540-260	39	1810	32
303-3	8	318-3CC	13	345-CC-375	11	357-CC	22	530M-087	30	1540-260-687	40	1820	32
303-3M	8	318-3CC-375	13	345-CC-375-PZ	26	357-RA	23	530M-141	30	1540-260-687	40	1830	32
304	8	320-1CC	13	345-CC-687	11	360-2D	12	530-1	30	1540-320	39	6421	32
304 PZ	25	320-2CC	13	345-SCC-PZ	26	361-CC	12	530-2	30	1540-320-687	40	7001	45
304-1	8	320-3CC	13	345-2CCPZ	26	361-CCST	18	531-1	30	1540-320-687	40	7002	45
304-1 PZ	25	320-CC-S	11	347-CC	16	362-CC	12	531-2	30	1540-320	39	7003	45
304-3	8	320-CC-S-PZ	26	347-CC-1 00	18	362-CCST	39	532	32	1540-320-687	40	7004	45
305	7	320-CC-T	19	347-CC-2	16	363	12	562-1	31	1540-320-687	40	7005	45
305-1	7	325-1CC	13	347-CC-375	16	363-CCST	18	562-2	31	1540-375	39	7006	45
307	8	325-2CC	13	347-CC-687	16	363-DS	21	562-3	31	1540-380	39	7104	47
307-M	8	325-3CC	13	348-1CC	13	364-CC	22	1350	46	1540-380-687	40	9001	44
307-PZ	25	325-CC-2-PZ	26	348-1CC-375	13	364-DS-CC	21	1355	46	1540-380-687	40	9002	44
307-1	8	325-CC-S	11	348-2CC	13	364-1-DS-CC	21	1370	46	1540-550	39	9003	44
307-1M	8	325-CC-T	19	348-2CC-375	13	365-CC	18	1375	46	1540-550-687	40	9004	44
307-1 PZ	25	328-PCE	24	348-3CC	13	368-1	10	1390	46	1540-550-687	40	9005	44
307-3 PZ	25	328-PC	24	348-3CC-375	13	368-2	10	1395	46	1540-687	40	9006	44
307-3	8	329-PC	24	348H-1CC	14	369-CC	14	1400	46	1540-687 O	40		
307-3M	8	329-PCE	24	348H-2CC	14	370	23	1405	46	1543	38	CABLES	
308-1	9	336-CC	16	348H-3CC	14	370-40	3	1450	47	1544	38	MICROPORE 190	52
308-3	9	336-CC-TAB	15	348-1CC-N	13	370-45	23	1470	47	1544-687	39	MICROFLEX 165	54-55
309-1	9	336-CC-1 000	16	348-2CC-N	13	370-F	23	1480	47	1544-687 O	39	MICROFLEX 150	56-57
309-2	9	336-CC-1 000-TAB	15	348-3CC-N	13	370-M	23	1505	41	1545-260	39	MICROFLEX 095	58-59
309-3	9	336-CC-2	16	348-1CC-T	13	372	10	1519-1	36	1545-320	39	MICROFORM 139	60-61
310-CC	20	336-CC-2-TAB	15	348-2CC-T	13	372-1	17	1519-1FLX	37	1545-375	39	MICROFORM 088	62-63
310-CC-2	20	336-CC-375	16	348-2CC-T	13	373-1 & 3	10	1519-2	36	1545-380	39	MICROFLEX 155	53
310-CC-375	20	336-CC-375-TAB	15	348V-1CC	14	375-CC-1, 2, 3	17	1519-2FLX	37	1545-550	39	MICROFLEX 098	64

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United Microwave
Products Inc.



United Microwave Products, Inc. was founded in 1975 and since then has become a leader in innovative connector design. Our commitment was and still is to price competitively, manufacture quality parts and deliver to negotiated dates. United Microwave rates our customers number one knowing that they significantly contribute to our success.

Originally, United Microwave Products Inc. started designing and manufacturing special RF connectors, cable assemblies, and associated microwave products. This specialization along with continued investment in high quality equipment makes United Microwave a viable source for all RF connector applications. We offer every product listed in this catalog at competitive prices and deliveries to meet customer requirements.

Please contact us or our representatives for additional product information and design applications.

WARRANTY

UNITED MICROWAVE WARRANTS
PRODUCTS OF ITS MANUFACTURE TO
BE FREE FROM DEFECTS IN
MATERIAL AND WORKMANSHIP
FOR A PERIOD OF ONE YEAR
UNDER NORMAL
USAGE CONDITIONS

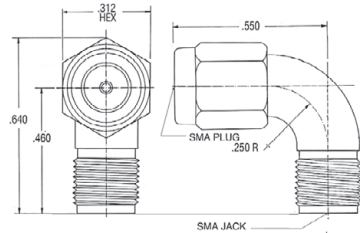
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PRECISION 90 ADAPTERS AT AFFORDABLE PRICING

STANDARD SMA PERFORMANCE DC to 18 GHz

MAX VSWR 1.20:1

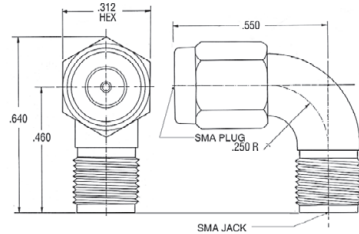


RADIUS RIGHT ANGLE SMA PLUG TO SMA JACK ADAPTER

PART NO	1-9	10-24	25-49	50-99	100+
370	\$28.50	\$26.75	\$25.25	\$23.50	\$22.75

HIGH PERFORMANCE SMA DC to 26.5 GHz

MAX VSWR 1.25:1

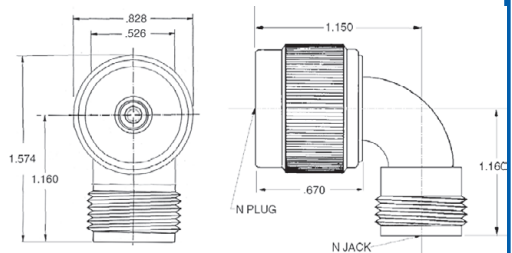


HIGH PERFORMANCE RADIUS RIGHT ANGLE SMA PLUG TO SMA JACK ADAPTER

PART NO	1-9	10-24	25-49	50-99	100+
370-26	\$37.50	\$34.50	\$31.75	\$29.25	\$27.50

HIGH PERFORMANCE TYPE "N" DC to 18 GHz

MAX VSWR 1.20:1

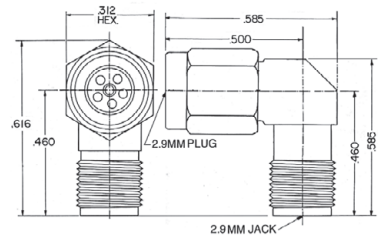


RADIUS RIGHT ANGLE TYPE "N" PLUG TO TYPE "N" JACK ADAPTER

PART NO	1-9	10-24	25-49	50-99	100+
1521	\$142.00	\$135.00	\$127.00	\$119.00	\$112.00

STANDARD PERFORMANCE 2.9mm DC to 40.0 GHz

MAX VSWR 1.25:1



RADIUS RIGHT ANGLE 2.9MM PLUG TO 2.9MM JACK ADAPTER

PART NO	1-9	10-24	25-49	50-99	100+
370-40	\$121.00	\$116.00	\$111.00	\$107.00	\$105.00

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SMA Connectors

The SMA Series Connectors listed on the following pages are available primarily of stainless steel construction. The stainless steel is normally gold plated. However, all connectors are available in passivated stainless steel and may be ordered by adding the suffix SF to the part number (SF = Stainless Finish). Almost all female panel mount and bulkhead connectors are available with captivated contacts. If captivation is required, add the letters CC to the part number (CC = Captive Contact). Figure 1.2 shows greater than 18GHz performance is possible at United Microwave (26 = 26GHz High performance).



Figure 1.1

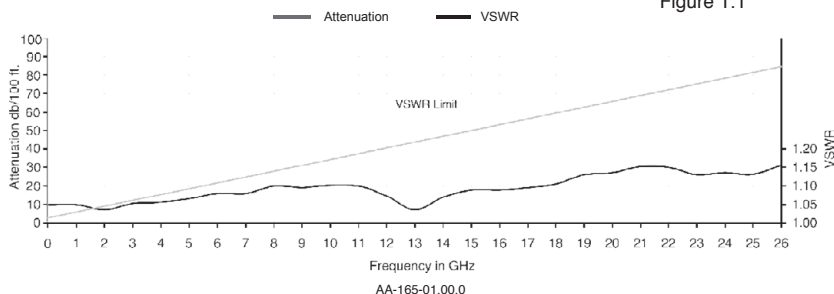
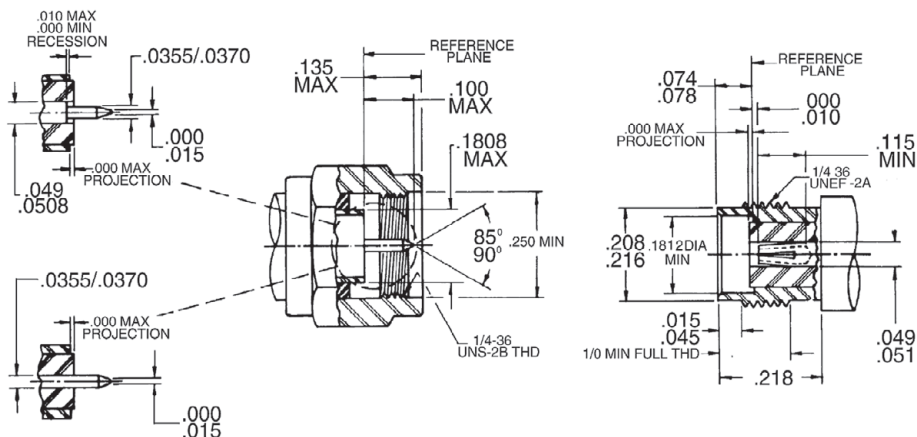


Figure 1.2 SMA PLUG to SMA PLUG ONE FOOT MICROFLEX 165 CABLE

Figure 1.3

SMA Interface Dimensions Per MIL-C-39012



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SMA Specifications Per MIL-C-39012

REQUIREMENT	MIL-C-39012 PARA	SPECIFICATIONS																																										
MATERIAL	3.3	Steel corrosion resistant per QQ-S-763, class 303, Beryllium Copper per QQ-C-530 condition HT Silicone Rubber per ZZ-R-765, class II B, Grade 65-75 TFE Fluorocarbon per L-P-403 Soft copper per QQ-B-825																																										
FINISH	3.31	Center contacts: 0.00005 min. gold per MIL-G-45204 type II Grade C over 0.0001 min. copper per MIL-C-14550. Other Metal parts: Sufficient to meet corrosion requirements PARA 3.14 of MIL-C-39012.																																										
DESIGN	3.4	Mating dimensions are in accordance with Figure 1.3																																										
INSULATION RESISTANCE	3.11	5,000 MEGOHMS minimum per MIL-STD-202, Method 302.																																										
DIELECTRIC WITHSTANDING VOLTAGE AND RF HIGH POTENTIAL	3.18	MIL-STD 202, Method 301. <table><tr><th>CABLES</th><th>VRMS @ 60CPS</th><th>VRMS @5MHz</th></tr><tr><td>RG-178, 122, 174, 179, 316,</td><td>500</td><td>335</td></tr><tr><td>.085 SR</td><td>750</td><td>500</td></tr><tr><td>RG-58, 142, 223, 303, .141 S, R,</td><td>1,000</td><td>670</td></tr></table>	CABLES	VRMS @ 60CPS	VRMS @5MHz	RG-178, 122, 174, 179, 316,	500	335	.085 SR	750	500	RG-58, 142, 223, 303, .141 S, R,	1,000	670																														
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.085 SR	750	500																																										
RG-58, 142, 223, 303, .141 S, R,	1,000	670																																										
CONTACT RESISTANCE (Millivolt Drop)	3.17	<table><tr><th colspan="2">Maximum millivolt drop</th></tr><tr><th>Initial</th><th>After</th></tr><tr><td>Center Contact 3.0</td><td>4.0</td></tr><tr><td>Outer Contact 2.0</td><td>Not applicable</td></tr><tr><td>Braid to Body 0.5</td><td>Not applicable</td></tr></table>	Maximum millivolt drop		Initial	After	Center Contact 3.0	4.0	Outer Contact 2.0	Not applicable	Braid to Body 0.5	Not applicable																																
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Outer Contact 2.0	Not applicable																																											
Braid to Body 0.5	Not applicable																																											
VOLTAGE STANDING WAVE RATIO (VSWR)	3.14	<table><tr><th colspan="3">Straight Plugs and Jacks</th></tr><tr><th>CABLES</th><th></th><th>VSWR</th></tr><tr><td>RG-178</td><td>1.20+0.025</td><td>(F) GHz</td></tr><tr><td>RG- 122, 174, 179 & 316</td><td>1.15+0.02</td><td>(F) GHz</td></tr><tr><td>RG-58, 142, 223 & 303</td><td>1.15+0.01</td><td>(F) GHz</td></tr><tr><td>.085 DIA. S.R. (RG-401)</td><td>1.15+0.01</td><td>(F) GHz</td></tr><tr><td>.141 DIA. S.R. (RG-402)</td><td>1.05+0.005</td><td>(F) GHz</td></tr><tr><th colspan="3">Right Angle Plugs and Jacks</th></tr><tr><th>CABLES</th><th></th><th>VSWR</th></tr><tr><td>RG-178</td><td>1.20+0.030</td><td>(F) GHz</td></tr><tr><td>RG- 122, 174, 179 & 316</td><td>1.15+0.03</td><td>(F) GHz</td></tr><tr><td>RG-58, 142, 223 & 303</td><td>1.15+0.02</td><td>(F) GHz</td></tr><tr><td>.085 DIA. S.R. (RG-401)</td><td>1.15+0.015</td><td>(F) GHz</td></tr><tr><td>.141 DIA. S.R. (RG-402)</td><td>1.05+0.01</td><td>(F) GHz</td></tr></table>	Straight Plugs and Jacks			CABLES		VSWR	RG-178	1.20+0.025	(F) GHz	RG- 122, 174, 179 & 316	1.15+0.02	(F) GHz	RG-58, 142, 223 & 303	1.15+0.01	(F) GHz	.085 DIA. S.R. (RG-401)	1.15+0.01	(F) GHz	.141 DIA. S.R. (RG-402)	1.05+0.005	(F) GHz	Right Angle Plugs and Jacks			CABLES		VSWR	RG-178	1.20+0.030	(F) GHz	RG- 122, 174, 179 & 316	1.15+0.03	(F) GHz	RG-58, 142, 223 & 303	1.15+0.02	(F) GHz	.085 DIA. S.R. (RG-401)	1.15+0.015	(F) GHz	.141 DIA. S.R. (RG-402)	1.05+0.01	(F) GHz
Straight Plugs and Jacks																																												
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.141 DIA. S.R. (RG-402)	1.05+0.01	(F) GHz																																										
INSERTION LOSS	3.29	Straight plugs and jacks, dB Max. = .05 x\GHz Freq. Right Angle plugs, dB Max. = .15x\GHz Freq.																																										
FORCE TO ENGAGE AND DISENGAGE	3.51	Longitudinal force is not applicable. torque 2 in-lbs. maximum.																																										
COUPLING NUT PROOF TORQUE	3.6	15 inch-pounds minimum.																																										

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SMA Specifications Per MIL-C-39012

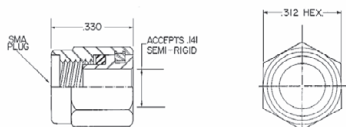
REQUIREMENT	MIL C 39012 PARA	SPECIFICATIONS			
CONNECTOR DURABILITY	3.16	Insertion and withdrawal 500 cycles min. at 12 Cycl/min. max Connector shall show no evidence of mechanical failure and shall meet the mating characteristics requirements.			
CABLE RETENTION FORCE	3.26	See Table I			
	TABLE 1 -Cable retention force.				
	Cable dielectric Outer diameter	Non crimp Single braid	Crimp Single braid		
		Center contact		Center contact	
		Captive Pounds (max)	Non Captive Pounds (max)	Captive Pounds (max)	Non Captive Pounds (max)
	Inches (max)				
	.036	13	10	13	10
	.066	25	20	25	20
	.110	35	30	35	30
.122	45	40	45	40	
MATING CHARACTERISTICS	3.7	Contacts with spring members Center contact (female) Oversize test pin - .0375 inches minimum diameter Test pin finish - 16 Insertion depth - .030/.045 inches Number of insertions - 3 Insertion force test: Steel test pin Diameter - .0370 inches minimum diameter Insertion depth - .050/.075 inches Test pin finish - 16 Insertion force - 3 Pounds maximum Withdrawal force test: Steel test pin Diameter - .0355 inches maximum diameter Insertion depth - .050/.075 inches Withdrawal force - 1 Ounce minimum Test pin finish - 16			
VIBRATION	3.18	MIL-STD-202, method 204, test condition B. No discontinuities.			
SHOCK	3.19	MIL-STD-202, method 213, test condition I. No discontinuities.			
THERMAL SHOCK	3.20	Refer to applicable military slash sheet or consult factory.			
CORROSION SALT SPRAY	3.13	MIL-STD-202, method 101, test condition B , the salt solution shall be 5 percent.			
MOISTURE RESISTANCE	3.23	MIL-STD-202, method 106. Insulation 200 MEGOHMS min. within 5 minutes after removal from humidity.			
CABLE RETENTION	3.24	Refer to applicable military slash sheet or consult factory.			
CORONA LEVEL	3.22	Refer to applicable military slash sheet or consult factory.			

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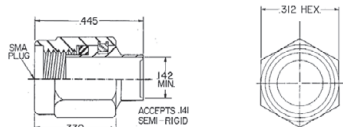
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SMA Connectors to Semi-Rigid Cable



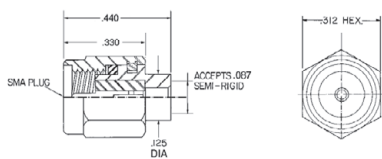
STRAIGHT PLUG .141 SEMI-RIGID

PART NO	1-9	10-24	25-49	50-99	100+
300-1	\$4.25	\$4.00	\$3.75	\$3.50	\$3.25



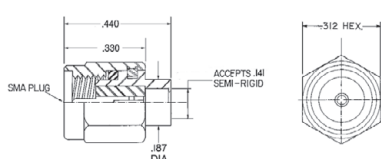
STRAIGHT PLUG .141 SEMI-RIGID IMPROVED SOLDER TYPE

PART NO	1-9	10-24	25-49	50-99	100+
300	\$4.25	\$4.00	\$3.75	\$3.50	\$3.25



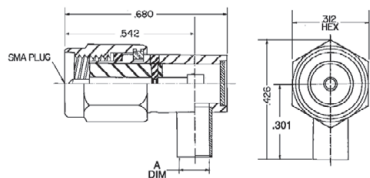
STRAIGHT PLUG .085 SEMI-RIGID WITH CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
301-1	\$4.75	\$4.50	\$4.25	\$4.00	\$3.75



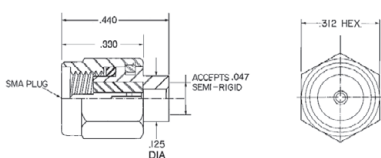
STRAIGHT PLUG .141 SEMI-RIGID WITH CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
300-7	\$4.75	\$4.50	\$4.25	\$4.00	\$3.75



RIGHT ANGLE PLUG DC-12.4 GHZ

PART NO	(A) DIM	CABLE	1-9	10-24	25-49	50-99	100+
305	.143	RG-402	\$15.00	\$14.75	\$13.75	\$12.75	\$12.50
305-1	.0875	RG-405	\$15.00	\$14.75	\$13.75	\$12.75	\$12.50



STRAIGHT PLUG .047 SEMI-RIGID WITH CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
301-3	\$12.75	\$12.50	\$12.25	\$12.00	\$11.75

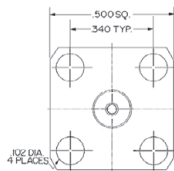
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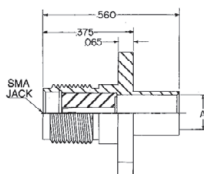
Prices listed effective as of 1 July 2008 and subject to change at any time.

SMA Connectors to Semi-Rigid Cable



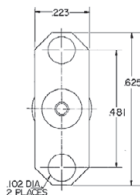
303

4 HOLE JACK SEMI-RIGID SOLDER TYPE

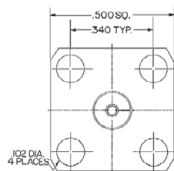


307

2 HOLE JACK SEMI-RIGID SOLDER TYPE

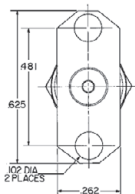
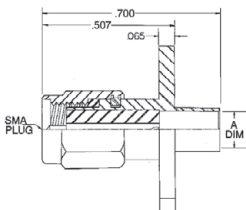


PART NO	(A) DIM	CABLE	1-9	10-24	25-49	50-99	100+
303	.143	141 SR	\$9.25	\$9.00	\$8.75	\$8.50	\$8.25
303-1	.0875	085 SR	\$9.25	\$9.00	\$8.75	\$8.50	\$8.25
303-3	.051	047 SR	\$10.25	\$10.00	\$9.75	\$9.50	\$9.25
307	.143	141 SR	\$9.75	\$9.50	\$9.25	\$9.00	\$8.75
307-1	.0875	085 SR	\$9.75	\$9.50	\$9.25	\$9.00	\$8.75
307-3	.051	047 SR	\$10.75	\$10.50	\$10.25	\$10.00	\$9.75



303-M

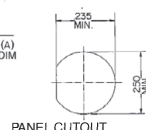
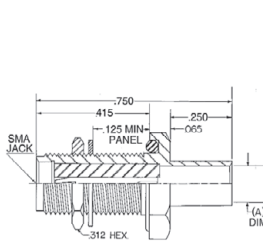
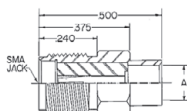
4 HOLE JACK SEMI-RIGID SOLDER TYPE



307-M

4 HOLE JACK SEMI-RIGID SOLDER TYPE

PART NO	(A) DIM	CABLE	1-9	10-24	25-49	50-99	100+
303M	.143	141 SR	\$20.00	\$19.75	\$18.75	\$17.75	\$17.50
303-1M	.0875	085 SR	\$21.00	\$20.75	\$20.50	\$20.25	\$19.25
303-3M	.051	047 SR	\$22.75	\$22.50	\$22.25	\$22.00	\$21.75
307M	.143	141 SR	\$20.75	\$20.50	\$20.25	\$20.00	\$19.75
307-1M	.0875	085 SR	\$22.75	\$22.50	\$22.25	\$22.00	\$21.75
307-3M	.051	047 SR	\$23.75	\$23.50	\$23.25	\$23.00	\$22.75



PANEL CUTOUT

STRAIGHT JACK SEMI-RIGID IMPROVED SOLDER TYPE

PART NO	(A) DIM	CABLE	1-9	10-24	25-49	50-99	100+
302	.143	141 SR	7.50	7.25	7.00	6.75	6.50
302-1	.0875	085 SR	7.50	7.25	7.00	6.75	6.50
302-3	.051	047 SR	18.25	17.50	16.75	16.25	15.75

D MOUNT BULKHEAD JACK SEMI-RIGID SOLDER TYPE

PART NO	(A) DIM	CABLE	1-9	10-24	25-49	50-99	100+
304	.143	141 SR	\$8.25	\$8.00	\$7.75	\$7.50	\$7.25
304-1	.0875	085 SR	\$8.25	\$8.00	\$7.75	\$7.50	\$7.25
304-3	.051	047 SR	\$24.50	\$23.50	\$23.25	\$23.00	\$22.50

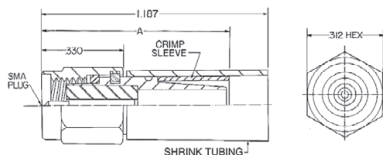
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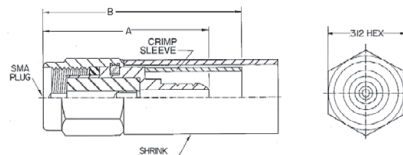
Prices listed effective as of 1 July 2008 and subject to change at any time.

SMA Connectors to Flexible Cables



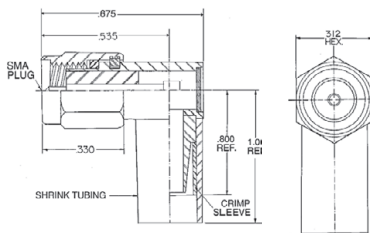
STRAIGHT CABLE PLUG SOLDER ATTACHMENT

PART NO.	A DIM.	CABLE	1-9	10-24	25-49	50-99	100+
351-1	.725(.775)	RG-55/U, 58, 141, 142, 223, 303, 400	\$7.49	\$6.97	\$6.49	\$5.99	\$5.49
351-3	.750(.775)	RG-174/U, 179, 187, 188, 316	\$7.49	\$6.97	\$6.49	\$5.99	\$5.49



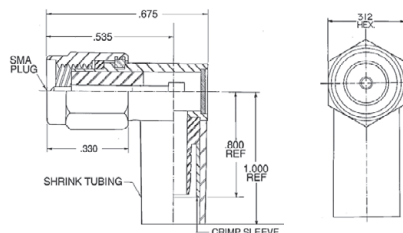
STRAIGHT CABLE PLUG CRIMP OR SOLDER ATTACHMENT

PART NO.	A DIM.	B DIM.	CABLE	1-9	10-24	25-49	50-99	100+
352-1	.690	.945	RG-55/U, 142, 223	\$7.49	\$6.97	\$6.49	\$5.99	\$5.49
352-2	.690	.945	RG-58, 141, 303, 400	\$7.49	\$6.97	\$6.49	\$5.99	\$5.49
352-3	.655	.815	RG-174/U, 179, 187, 188, 316	\$7.49	\$6.97	\$6.49	\$5.99	\$5.49



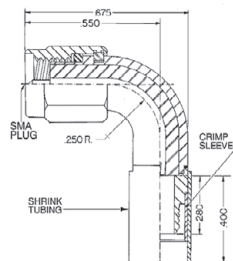
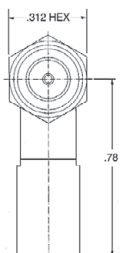
RIGHT ANGLE PLUG SOLDER ATTACHMENT

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
308-1	RG-55/U, 58, 141, 142, 223, 303, 400	\$15.00	\$14.75	\$13.75	\$12.75	\$12.50
308-3	RG-174/U, 179, 187, 188, 316	\$15.00	\$14.75	\$13.75	\$12.75	\$12.50



RIGHT ANGLE PLUG CRIMP OR SOLDER ATTACHMENT

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
309-1	RG-55/U, 142, 223	\$15.00	\$14.75	\$13.75	\$12.75	\$12.50
309-2	RG-58, 141, 303, 400	\$15.00	\$14.75	\$13.75	\$12.75	\$12.50
309-3	RG-174/U, 179, 187, 188, 316	\$15.00	\$14.75	\$13.75	\$12.75	\$12.50

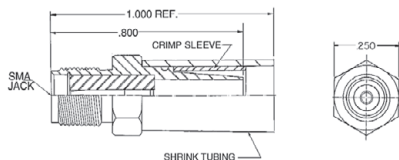


SMA RADIUS RIGHT ANGLE PLUG SOLDER/CRIMP ATTACHMENT FOR RG-55/U, 58, 141, 142, 223, 303 & 400 CABLES

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
314	RG-55/U, 58, 141, 142, 223, 303, 400	\$42.75	\$39.50	\$37.25	\$34.50	\$29.50

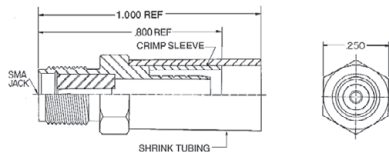
Prices listed effective as of 1 July 2008 and subject to change at any time.

SMA Connectors to Flexible Cables



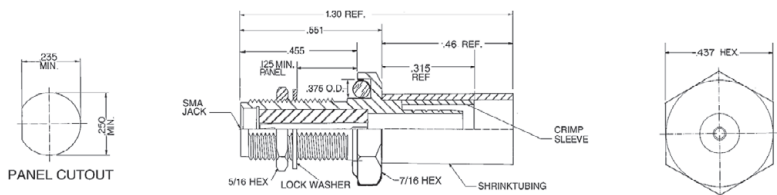
STRAIGHT CABLE JACK SOLDER ATTACHMENT

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
368-1	RG-55/U, 58, 141, 142, 223, 303, 400	\$10.50	\$10.00	\$9.50	\$9.00	\$8.25
368-3	RG-174/U, 179, 187, 188, 316	\$10.50	\$10.00	\$9.50	\$9.00	\$8.25



STRAIGHT CABLE JACK CRIMP OR SOLDER ATTACHMENT

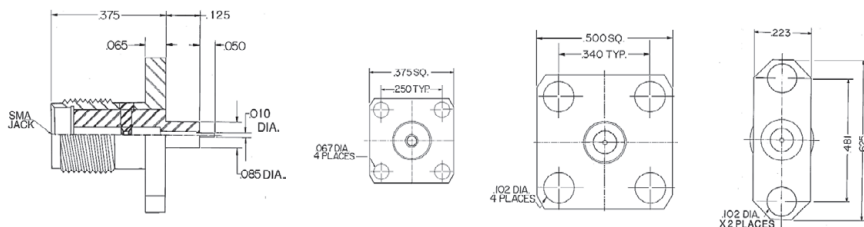
PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
373-1	RG-55/U, 58, 141, 142, 223, 303, 400	\$10.50	\$10.00	\$9.50	\$9.00	\$8.25
373-3	RG-174/U, 179, 187, 188, 316	\$10.50	\$10.00	\$9.50	\$9.00	\$8.25



D MOUNT BULKHEAD CABLE JACK CRIMP/SOLDER ATTACHMENT

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
386-1	RG-55/U 142, 223	\$12.20	\$11.59	\$11.01	\$10.46	\$ 9.41
386-2	RG-58, 141, 303, 400	\$12.20	\$11.59	\$11.01	\$10.46	\$9.41
386-3	RG-174/U, 179, 187, 188, 316	\$12.20	\$11.59	\$11.01	\$10.46	\$9.41

SMA Flange Mount Jack Captive Contact • .010 Microstrip Terminal



SMA 2 or 4 HOLE FLANGE JACK CAPTIVE CONTACT .010 MICROSTRIP

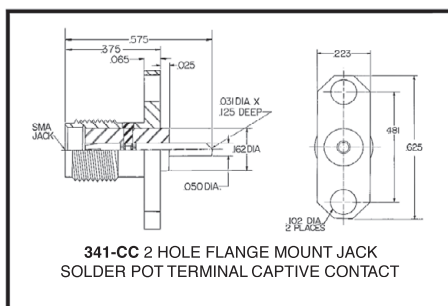
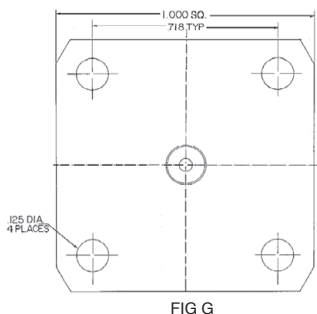
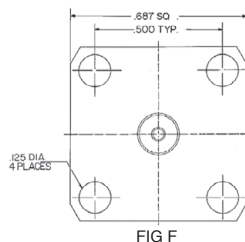
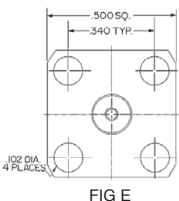
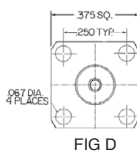
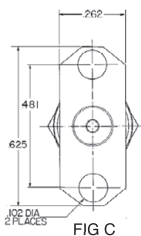
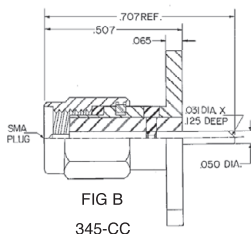
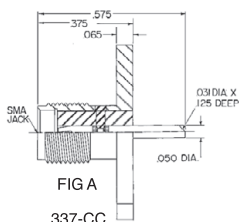
PART NO	FLANGE	1-9	10-24	25-49	50-99	100+
344-CC	SMA .500 SQ.	\$8.75	\$8.50	\$8.25	\$7.50	\$7.00
344-2-CC	SMA 2 HOLE	\$9.25	\$9.00	\$8.75	\$8.00	\$7.50
344-375-CC	SMA .375 SQ.	\$8.75	\$8.50	\$8.25	\$7.50	\$7.00

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SMA • Panel Panel Mount • Solder Pot Terminal • Captive Contact



SMA JACK FLANGE MOUNT SOLDER POT TERMINAL CAPTIVE CONTACT

345CC FIG - B (SMA PLUG)

PART NO.	FLANGE SIZE	FIGURE	1-9	10-24	25-49	50-99	100+
345-CC-375	.375 SQ.	D	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35
345-CC-2	2 HOLE	C	\$10.25	\$9.80	\$9.25	\$8.75	\$8.25
345-CC	.500 SQ.	E	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35
345-CC-687	.687 SQ.	F	\$17.50	\$16.75	\$15.50	\$14.75	\$14.25
345-CC-1.00	1.000 SQ.	G	\$21.75	\$20.75	\$20.25	\$20.10	\$19.95

337CC FIG - A (SMA JACK)

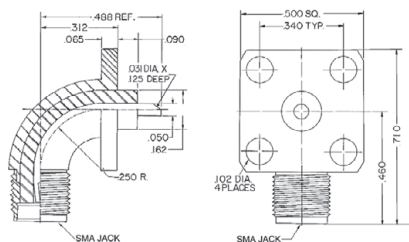
PART NO.	FLANGE SIZE	FIGURE	1-9	10-24	25-49	50-99	100+
337-CC-375	.375 SQ.	D	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24
341-CC	2 HOLE	H	\$6.95	\$6.31	\$5.73	\$5.21	\$4.74
337-CC	.500 SQ.	E	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24
320-CC-S	.687 SQ.	F	\$7.45	\$6.75	\$6.25	\$5.75	\$5.25
325-CC-S	1.000 SQ.	G	\$11.75	\$10.75	\$10.25	\$10.10	\$9.95

For non-captive contact, delete the "CC" designator.
Add the suffix SF for passivated stainless finish.
Suffix BR for brass body with a Hard Nickel Finish.

BR (brass body) unavailable for
ALL SMA MALE (PLUG) CONNECTORS!
ALL PRICES STATED ARE FOR GOLD
FINISH PLEASE CONSULT FACTORY FOR
STAINLESS FINISH OR BRASS BODY
STYLE.

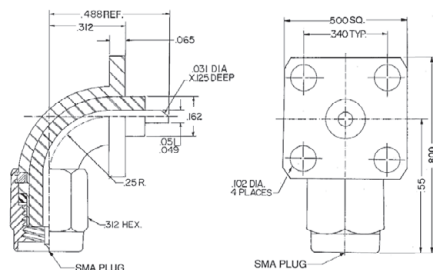
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SMA Right Angle Panel Mount Solder Pot Terminal



4 HOLE RADIUS RIGHT ANGLE JACK

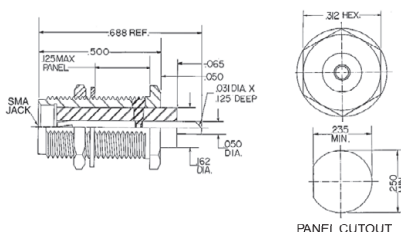
PART NO	1-9	10-24	25-49	50-99	100+
377	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50



4 HOLE RADIUS RIGHT ANGLE PLUG

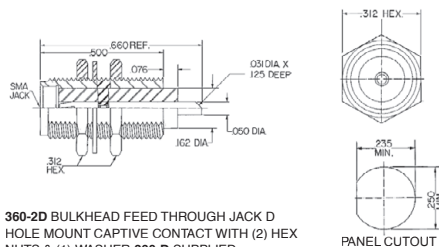
PART NO	1-9	10-24	25-49	50-99	100+
372	\$41.17	\$39.06	\$37.11	\$35.26	\$31.73

SMA Bulkhead Mount Solder Pot Terminal



BULKHEAD FEED THROUGH JACK D HOLE MOUNT CAPTIVE CONTACT

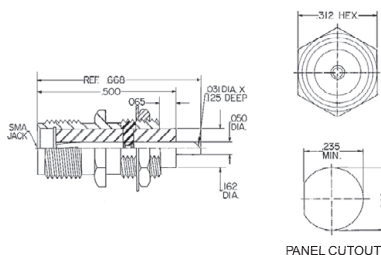
PART NO	1-9	10-24	25-49	50-99	100+
362-CC	\$6.75	\$6.50	\$6.25	\$5.75	\$5.50
362-CC-SF	\$6.25	\$6.00	\$5.75	\$5.25	\$5.00



360-2D BULKHEAD FEED THROUGH JACK D HOLE MOUNT CAPTIVE CONTACT WITH (2) HEX NUTS & (1) WASHER 360-D SUPPLIED WITHOUT ANY HARDWARE 360 SUPPLIED WITH SINGLE NUT & WASHER

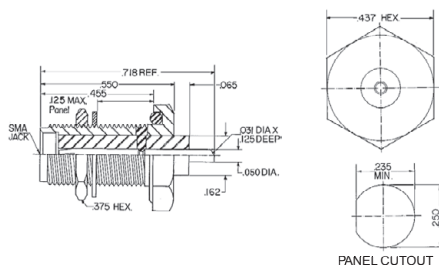
PART NO	1-9	10-24	25-49	50-99	100+
360-2D-CC	\$8.00	\$7.75	\$7.50	\$7.25	\$6.75
360-2D-CC-SF	\$7.50	\$7.25	\$7.00	\$6.75	\$6.25
360-D-CC	\$7.90	\$7.65	\$7.40	\$7.15	\$6.65
360-D-CC-SF	\$7.40	\$7.15	\$6.90	\$6.65	\$6.15
360-CC	\$7.80	\$7.65	\$7.30	\$7.05	\$6.55
360-CC-SF	\$7.30	\$7.15	\$6.80	\$6.45	\$6.05

The suffix SF is for passivated stainless finish. Or consult factory for brass body nickel finish pricing.



BULKHEAD FEED THROUGH JACK D HOLE MOUNT FRONT CAPTIVE CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
363-CC	\$6.75	\$6.50	\$6.25	\$5.75	\$5.50
363-CC-SF	\$6.25	\$6.00	\$5.75	\$5.25	\$5.00



BULKHEAD FEED THROUGH JACK D HOLE MOUNT "O" RING CAPTIVE CONTACT

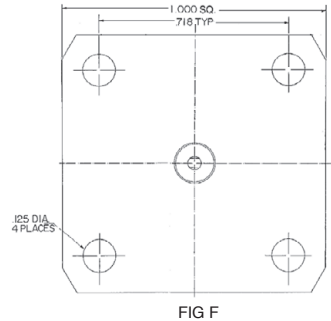
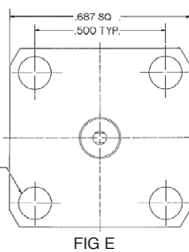
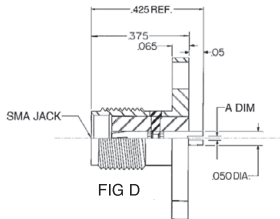
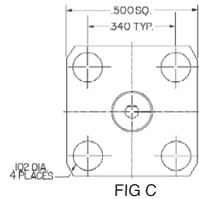
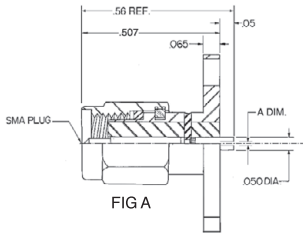
PART NO	1-9	10-24	25-49	50-99	100+
361-CC	\$10.25	\$10.00	\$9.75	\$9.00	\$8.25
361-CC-SF	\$9.75	\$9.50	\$9.25	\$8.50	\$7.75

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SMA Plug SMA Jack Flange Mount Slot Terminal Captive Contact



The suffix SF is for passivated stainless finish.

For non-captive contact connectors or brass connectors with a Hard Nickel Finish consult factory for pricing
BRASS IS UNAVAILABLE FOR ALL SMA MALE PLUG CONNECTORS!

(FIG A) SMA PLUG BODY									
PART NO	FIG	ADIM	FLANGE	1-9	10-24	25-49	50-99	100+	
348-1CC-375	FIG B	.012	.375	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35	
348-1CC-375-SF	FIG B	.012	.375	\$9.00	\$8.55	\$8.00	\$7.45	\$6.85	
348-2CC-375	FIG B	.018	.375	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35	
348-2CC-375-SF	FIG B	.018	.375	\$9.00	\$8.55	\$8.00	\$7.45	\$6.85	
348-3CC-375	FIG B	.028	.375	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35	
348-3CC-375-SF	FIG B	.028	.375	\$9.00	\$8.55	\$8.00	\$7.45	\$6.85	
348-1CC	FIG C	.012	.500	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35	
348-1CC-SF	FIG C	.012	.500	\$9.00	\$8.55	\$8.00	\$7.45	\$6.85	
348-2CC	FIG C	.018	.500	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35	
348-2CC-SF	FIG C	.018	.500	\$9.00	\$8.55	\$8.00	\$7.45	\$6.85	
348-3CC	FIG C	.028	.500	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35	
348-3CC-SF	FIG C	.028	.500	\$9.00	\$8.55	\$8.00	\$7.45	\$6.85	
348-1CC-T	FIG E	.012	.687	\$18.00	\$17.45	\$16.00	\$15.25	\$14.75	
348-1CC-T-SF	FIG E	.012	.687	\$17.50	\$16.95	\$15.50	\$14.75	\$14.25	
348-2CC-T	FIG E	.018	.687	\$18.00	\$17.45	\$16.00	\$15.25	\$14.75	
348-2CC-T-SF	FIG E	.018	.687	\$17.50	\$16.95	\$15.50	\$14.75	\$14.25	
348-3CC-T	FIG E	.028	.687	\$18.00	\$17.45	\$16.00	\$15.25	\$14.75	
348-3CC-T-SF	FIG E	.028	.687	\$17.50	\$16.95	\$15.50	\$14.75	\$14.25	
348-1CC-N	FIG F	.012	1.000	\$21.75	\$20.75	\$20.25	\$20.10	\$19.95	
348-1CC-N-SF	FIG F	.012	1.000	\$21.25	\$20.25	\$19.75	\$19.60	\$19.45	
348-2CC-N	FIG F	.018	1.000	\$21.75	\$20.75	\$20.25	\$20.10	\$19.95	
348-2CC-N-SF	FIG F	.018	1.000	\$21.25	\$20.25	\$19.75	\$19.60	\$19.45	
348-3CC-N	FIG F	.028	1.000	\$21.75	\$20.75	\$20.25	\$20.10	\$19.95	
348-3CC-N-SF	FIG F	.028	1.000	\$21.25	\$20.25	\$19.75	\$19.60	\$19.45	

(FIG D) SMA JACK BODY									
PART NO	FIG	ADIM	FLANGE	1-9	10-24	25-49	50-99	100+	
318-1CC-375	FIG B	.012	.375	\$6.95	\$6.31	\$5.73	\$5.21	\$4.74	
318-1CC-375-SF	FIG B	.012	.375	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24	
318-2CC-375	FIG B	.018	.375	\$6.95	\$6.31	\$5.73	\$5.21	\$4.74	
318-2CC-375-SF	FIG B	.018	.375	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24	
318-3CC-375	FIG B	.028	.375	\$6.95	\$6.31	\$5.73	\$5.21	\$4.74	
318-3CC-375-SF	FIG B	.028	.375	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24	
318-1CC	FIG C	.012	.500	\$6.95	\$6.31	\$5.73	\$5.21	\$4.74	
318-1CC-SF	FIG C	.012	.500	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24	
318-2CC	FIG C	.018	.500	\$6.95	\$6.31	\$5.73	\$5.21	\$4.74	
318-2CC-SF	FIG C	.018	.500	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24	
318-3CC	FIG C	.028	.500	\$6.95	\$6.31	\$5.73	\$5.21	\$4.74	
318-3CC-SF	FIG C	.028	.500	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24	
320-1CC	FIG E	.012	.687	\$7.95	\$7.25	\$6.75	\$6.25	\$5.75	
320-1CC-SF	FIG E	.012	.687	\$7.45	\$6.75	\$6.25	\$5.75	\$5.25	
320-2CC	FIG E	.018	.687	\$7.95	\$7.25	\$6.75	\$6.25	\$5.75	
320-2CC-SF	FIG E	.018	.687	\$7.45	\$6.75	\$6.25	\$5.75	\$5.25	
320-3CC	FIG E	.028	.687	\$7.95	\$7.25	\$6.75	\$6.25	\$5.75	
320-3CC-SF	FIG E	.028	.687	\$7.45	\$6.75	\$6.25	\$5.75	\$5.25	
325-1CC	FIG F	.012	1.000	\$12.25	\$11.45	\$10.75	\$10.60	\$10.45	
325-1CC-SF	FIG F	.012	1.000	\$11.75	\$10.95	\$10.25	\$10.10	\$9.95	
325-2CC	FIG F	.018	1.000	\$12.25	\$11.45	\$10.75	\$10.60	\$10.45	
325-2CC-SF	FIG F	.018	1.000	\$11.75	\$10.95	\$10.25	\$10.10	\$9.95	
325-3CC	FIG F	.028	1.000	\$12.25	\$11.45	\$10.75	\$10.60	\$10.45	
325-3CC-SF	FIG F	.028	1.000	\$11.75	\$10.95	\$10.25	\$10.10	\$9.95	

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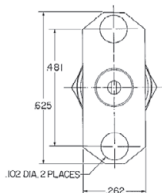
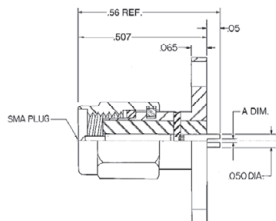
13 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pachell.net 13

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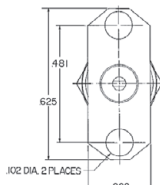
SMA 2 Hole Plug Flange Mount Slot Terminal Captive Contact

348 TABULATED

For non-captive contact, passivated stainless finish or brass body with a hard nickel finish body type. consult factory for pricing.



VERTICAL



HORIZONTAL

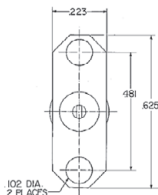
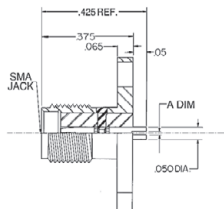
SMA 2 HOLE PLUG PANEL MOUNT SLOT

PART NO.	SLOT WIDTH A	SLOT POSITION	1-9	10-24	25-49	50-99	100+
348H-1CC	.012	HORIZONTAL	\$9.75	\$9.27	\$8.85	\$8.25	\$7.55
348H-2CC	.018	HORIZONTAL	\$9.75	\$9.27	\$8.85	\$8.25	\$7.55
348H-3CC	.028	HORIZONTAL	\$9.75	\$9.27	\$8.85	\$8.25	\$7.55
348V-1CC	.012	VERTICAL	\$9.75	\$9.27	\$8.85	\$8.25	\$7.55
348V-2CC	.018	VERTICAL	\$9.75	\$9.27	\$8.85	\$8.25	\$7.55
348V-3CC	.028	VERTICAL	\$9.75	\$9.27	\$8.85	\$8.25	\$7.55

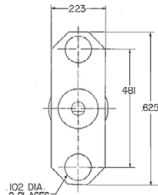
SMA 2 Hole Jack Flange Mount Slot Terminal Captive Contact

318 TABULATED

For non-captive contact, passivated stainless finish or brass body with a hard nickel finish body type. consult factory for pricing.



VERTICAL



HORIZONTAL

SMA 2 HOLE JACK PANEL MOUNT SLOT

PART NO.	SLOT WIDTH A	SLOT POSITION	1-9	10-24	25-49	50-99	100+
318H-1CC	.012	HORIZONTAL	\$6.75	\$6.10	\$5.70	\$5.20	\$4.75
318H-2CC	.018	HORIZONTAL	\$6.75	\$6.10	\$5.70	\$5.20	\$4.75
318H-3CC	.028	HORIZONTAL	\$6.75	\$6.10	\$5.70	\$5.20	\$4.75
318V-1CC	.012	VERTICAL	\$6.75	\$6.10	\$5.70	\$5.20	\$4.75
318V-2CC	.018	VERTICAL	\$6.75	\$6.10	\$5.70	\$5.20	\$4.75
318V-3CC	.028	VERTICAL	\$6.75	\$6.10	\$5.70	\$5.20	\$4.75

United Microwave Products Inc.

Direct Sales, Tech Support and Current Order Status

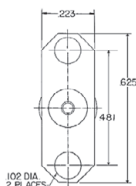
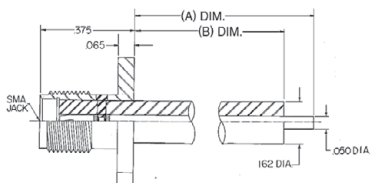
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SMA Jack Flange Mount Extended Terminal Captive Contact

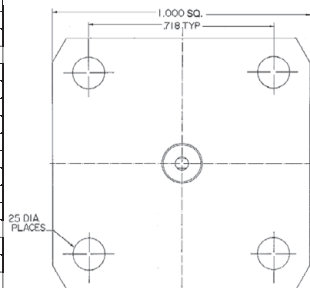
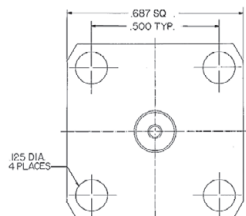
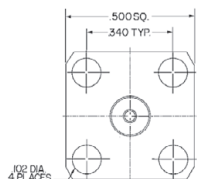
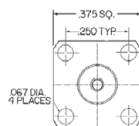
336-CC-CC 80 through 88 TABULATED

For non-captive contact, passivated stainless finish or brass body with a hard nickel finish body type. consult factory for pricing.



SMA 4 HOLE AND 2 HOLE FLANGE PANEL MOUNT EXTENDED STRAIGHT TERMINAL

336-CC-2 TAB						
FLANGE SIZE SMA 2 HOLE						
PART NO.	A DIM.	B DIM.	1 - 9	10 - 24	25 - 49	50 - 99
336-CC-2-80	.300	.090	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-2-81	.230	.110	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-2-82	.245	.110	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-2-83	.300	.145	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-2-84	.375	.175	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-2-85	.260	.200	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-2-86	.290	.210	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-2-87	.290	.240	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-2-88	.475	.375	\$7.50	\$7.25	\$7.00	\$6.25
336-CC-375 TAB						
FLANGE SIZE .375 SQUARE						
336-CC-375-80	.300	.090	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-375-81	.230	.110	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-375-82	.245	.110	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-375-83	.300	.145	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-375-84	.375	.175	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-375-85	.260	.200	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-375-86	.290	.210	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-375-87	.290	.240	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-375-88	.475	.240	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500 TAB						
FLANGE SIZE .500 SQUARE						
336-CC-500-80	.300	.090	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500-81	.230	.110	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500-82	.245	.110	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500-83	.300	.145	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500-84	.375	.175	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500-85	.260	.200	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500-86	.290	.210	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500-87	.290	.240	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-500-88	.475	.375	\$7.25	\$7.00	\$6.75	\$5.75
336-CC-687 TAB						
FLANGE SIZE .687 SQUARE						
336-CC-687-80	.300	.090	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-687-81	.230	.110	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-687-82	.245	.110	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-687-83	.300	.145	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-687-84	.375	.175	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-687-85	.260	.200	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-687-86	.290	.210	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-687-87	.290	.240	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-687-88	.475	.375	\$7.95	\$7.50	\$7.25	\$6.25
336-CC-1.000 TAB						
FLANGE SIZE 1.000 SQUARE						
336-CC-1.000-80	.300	.090	\$12.50	\$11.25	\$10.50	\$9.95
336-CC-1.000-81	.230	.110	\$12.50	\$11.25	\$10.50	\$9.95
336-CC-1.000-82	.245	.110	\$12.50	\$11.25	\$10.50	\$9.95
336-CC-1.000-83	.300	.145	\$12.50	\$11.25	\$10.50	\$9.95
336-CC-1.000-84	.375	.175	\$12.50	\$11.25	\$10.50	\$9.95
336-CC-1.000-85	.260	.200	\$12.50	\$11.25	\$10.50	\$9.95
336-CC-1.000-86	.290	.210	\$12.50	\$11.25	\$10.50	\$9.95
336-CC-1.000-87	.290	.240	\$12.50	\$11.25	\$10.50	\$9.95
336-CC-1.000-88	.475	.375	\$12.50	\$11.25	\$10.50	\$9.95



United Microwave Products Inc.

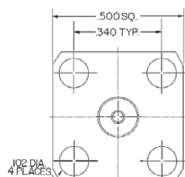
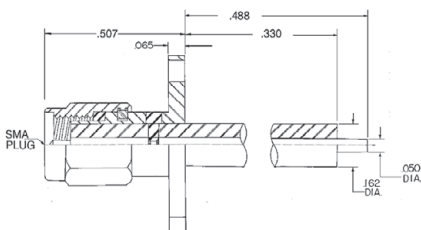
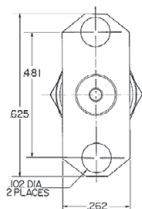
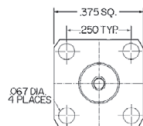
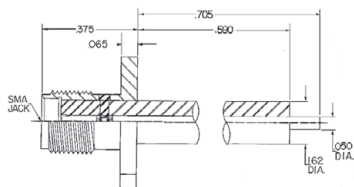
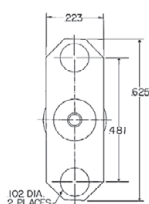
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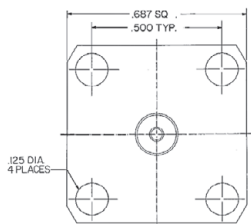
SMA Flange Mount Jack • Plug • Extended Terminal • Captive Contact

For non-captive contact or brass body with a hard nickel finish body type, consult factory for pricing.



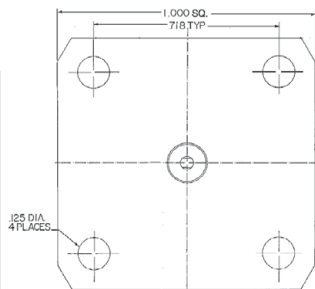
SMA JACK 4 HOLE PANEL MOUNT EXTENDED STRAIGHT TERMINAL

336-CC-(TABULATED)						
PART NO	FLANGE	1-9	10-24	25-49	50-99	100+
336-CC-2	2-HOLE	\$8.00	\$7.75	\$7.50	\$7.00	\$6.75
336-CC-2-SF	2-HOLE	\$7.50	\$7.25	\$7.00	\$6.50	\$6.25
336-CC-375	.375 SQ	\$7.75	\$7.50	\$7.25	\$6.75	\$5.75
336-CC-375-SF	.375 SQ	\$7.25	\$7.00	\$6.75	\$6.25	\$5.25
336-CC	.500 SQ	\$7.75	\$7.50	\$7.25	\$6.75	\$5.75
336-CC-SF	.500 SQ	\$7.25	\$7.00	\$6.75	\$6.25	\$5.25
336-CC-687	.687 SQ	\$8.45	\$8.00	\$7.75	\$7.25	\$6.75
336-CC-687-SF	.687 SQ	\$7.95	\$7.50	\$7.25	\$6.75	\$6.25
336-CC-1.000	1.000 SQ	\$13.00	\$11.75	\$11.00	\$10.70	\$9.95
336-CC-1.000-SF	1.000 SQ	\$12.50	\$11.25	\$10.50	\$10.20	\$9.45



SMA PLUG 4 HOLE PANEL MOUNT EXTENDED STRAIGHT TERMINAL

347-CC-(TABULATED)						
PART NO	FLANGE	1-9	10-24	25-49	50-99	100+
347-CC-2	2-HOLE	\$10.75	\$10.30	\$9.75	\$9.25	\$8.50
347-CC-2-SF	2-HOLE	\$10.25	\$9.80	\$9.25	\$8.75	\$8.25
347-CC-375	.375 SQ	\$10.25	\$9.77	\$9.35	\$8.75	\$8.15
347-CC-375-SF	.375 SQ	\$9.75	\$9.27	\$8.85	\$8.25	\$7.65
347-CC	.500 SQ	\$10.25	\$9.77	\$9.35	\$8.75	\$8.15
347-CC-SF	.500 SQ	\$9.75	\$9.27	\$8.85	\$8.25	\$7.65
347-CC-687	.687 SQ	\$18.00	\$17.25	\$16.00	\$15.25	\$14.75
347-CC-687-SF	.687 SQ	\$17.50	\$16.75	\$15.50	\$14.75	\$14.25
347-CC-1.000	1.000 SQ	\$22.25	\$21.25	\$20.75	\$20.60	\$20.45
347-CC-1.000-SF	1.000 SQ	\$21.75	\$20.75	\$20.25	\$20.10	\$19.95



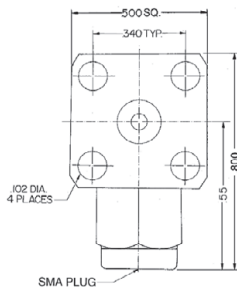
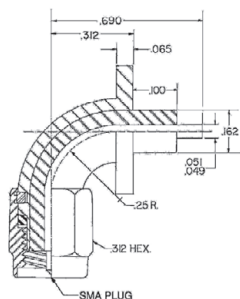
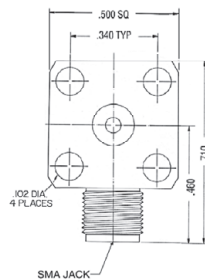
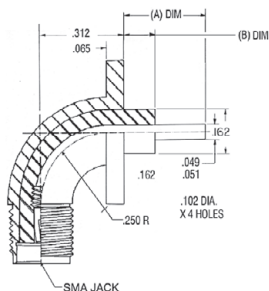
United Microwave Products Inc.

Direct Sales, Tech Support and Current Order Status

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SMA Flange Mount • Radius Right Angles • Extended Terminal



375-CC-(TABULATED) RADIUS RIGHT ANGLE JACK SMA 4 HOLE PANEL MOUNT CAPTIVE CONTACT EXTENDED STRAIGHT TERMINAL

PART NO.	A DIM.	B DIM.	1 - 9	10 - 24	25 - 49	50 - 99	100 +
375-CC-1	.310	.000	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50
375-CC-2	.074	.000	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50
375-CC-3	.100	.000	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50
375-CC-4	.050	.000	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50
375-CC-5	.250	.000	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50
375-CC-6	.400	.000	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50
375-CC-7	.460	.000	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50
376-CC	.300	.100	\$35.50	\$33.70	\$32.04	\$30.45	\$27.50
379-CC	.705	.590	\$45.00	\$41.50	\$37.25	\$34.50	\$31.40

372-1 4 HOLE RADIUS RIGHT ANGLE PLUG PANEL MOUNT EXTENDED STRAIGHT TERMINAL

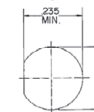
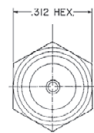
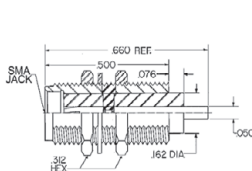
PART NO.	1 - 9	10 - 24	25 - 49	50 - 99	100 +
372-1	\$41.17	\$39.06	\$37.11	\$35.26	\$31.73

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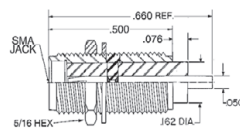
SMA Jack • Bulkhead Mount • Extended Terminal • Captive Contact



PANEL CUTOUT

BULKHEAD FEED THROUGH JACK D HOLE MOUNT CAPTIVE CONTACT

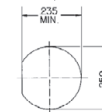
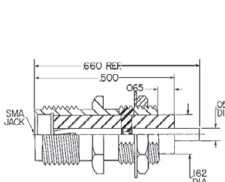
PART NO	1-9	10-24	25-49	50-99	100+
369-CC	\$8.50	\$8.25	\$8.00	\$7.75	\$7.25
369-CC-SF	\$8.00	\$7.75	\$7.50	\$7.25	\$6.75



PANEL CUTOUT

BULKHEAD .250 HOLE MOUNT FEED THROUGH JACK CAPTIVE CONTACT

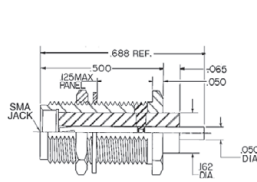
PART NO	1-9	10-24	25-49	50-99	100+
365-CC	\$8.00	\$7.75	\$7.50	\$7.25	\$6.75
365-CC-SF	\$7.50	\$7.25	\$7.00	\$6.75	\$6.25



PANEL CUTOUT

BULKHEAD JACK D HOLE MOUNT CAPTIVE CONTACT

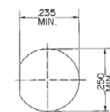
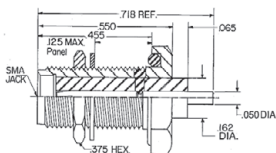
PART NO	1-9	10-24	25-49	50-99	100+
363-CCST	\$8.35	\$7.95	\$7.75	\$7.30	\$6.80
363-CCST-SF	\$7.85	\$7.45	\$7.25	\$6.80	\$6.30



PANEL CUTOUT

BULKHEAD FEED THROUGH JACK D HOLE MOUNT CAPTIVE CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
362-CCST	\$7.25	\$7.00	\$6.75	\$6.50	\$6.25
362-CCST-SF	\$6.75	\$6.50	\$6.25	\$6.00	\$5.75



PANEL CUTOUT

BULKHEAD FEED THROUGH JACK D HOLE MOUNT "O" RING CAPTIVE CONTACT

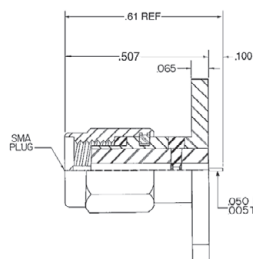
PART NO	1-9	10-24	25-49	50-99	100+
361-CCST	\$10.25	\$10.00	\$9.75	\$9.50	\$9.25
361-CCST-SF	\$9.75	\$9.50	\$9.25	\$9.00	\$8.75

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SMA • Flange Mount • Tab Terminal • Captive Contact



SMA PLUG TAB

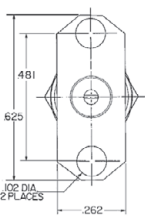


FIG A

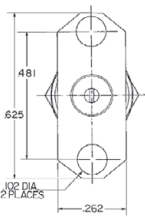


FIG B

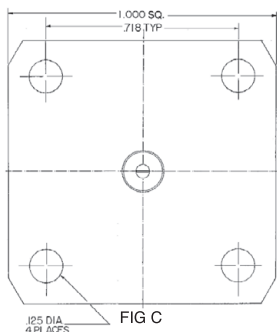
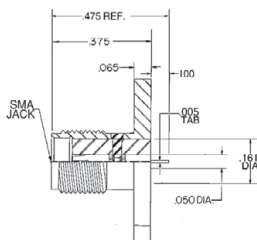


FIG C



SMA JACK TAB

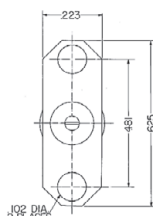


FIG D

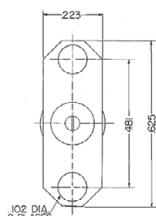


FIG E

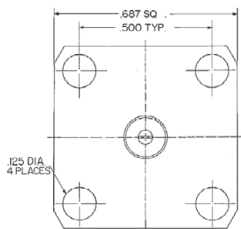


FIG F

349-TABULATED SMA 2 & 4 HOLE PANEL MOUNT TAB TERMINAL

349-CC (TABULATED) SMA PLUG

PART NO	FLANGE	FIG	1-9	10-24	25-49	50-99	100+
349-2-CC-H	2 HOLE	FIG A	\$9.75	\$9.27	\$8.85	\$8.25	\$7.55
349-2-CC-V	2 HOLE	FIG B	\$9.75	\$9.27	\$8.85	\$8.25	\$7.55
349-CC-375	.375 SQ	FIG H	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35
349-CC	.500 SQ	FIG G	\$9.50	\$9.05	\$8.50	\$7.95	\$7.35
349-CC-T	.687 SQ	FIG F	\$17.50	\$16.75	\$15.50	\$14.75	\$14.25
349-CC-N	1.000 SQ	FIG C	\$21.75	\$20.75	\$20.25	\$20.10	\$19.95

340-TABULATED SMA 2 & 4 HOLE PANEL MOUNT TAB TERMINAL

320-CC-T, 325-CC-T and 340-CC (TABULATED) SMA JACK

PART NO.	FLANGE	FIG	1-9	10-24	25-49	50-99	100+
340-2-CC-H	2 HOLE	FIG D	\$6.75	\$6.50	\$6.25	\$5.75	\$4.75
340-2-CC-V	2 HOLE	FIG E	\$6.75	\$6.50	\$6.25	\$5.75	\$4.75
340-CC-375	.375 SQ	FIG H	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24
340-CC	.500 SQ	FIG G	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24
320-CC-T	.687 SQ	FIG F	\$7.45	\$6.75	\$6.25	\$5.75	\$5.25
325-CC-T	1.000 SQ	FIG C	\$11.75	\$10.75	\$10.25	\$10.10	\$9.95

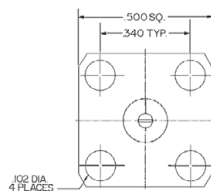


FIG G

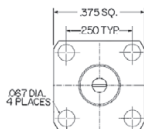


FIG H

For non-captive contact, passivated stainless finish or brass body with a hard nickel finish body type. consult factory for pricing.

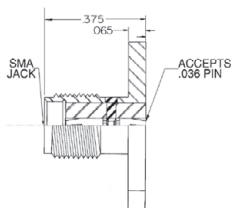
United Microwave Products Inc.

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19 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 19

Prices listed effective as of 1 July 2008 and subject to change at any time.

SMA • Flange Mount • Socket Terminal • Captive Contact



310-CC SMA JACK SOCKET TERMINAL

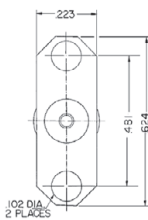


FIG A

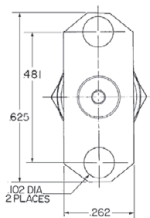
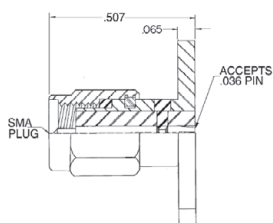


FIG B



312-CC SMA PLUG SOCKET TERMINAL

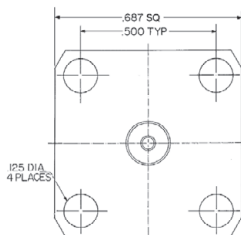


FIG C

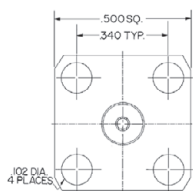


FIG D

310 TABULATED JACK 312 TABULATED PLUG

For non-captive contact, passivated stainless finish or brass body with a hard nickel finish body type. consult factory for pricing.

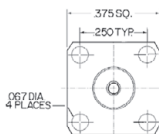


FIG E

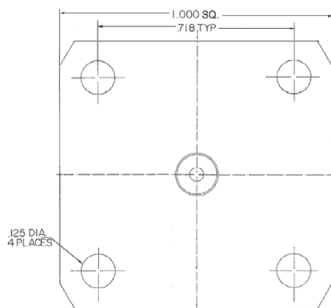


FIG F

310-CC TABULATED SMA JACK SOCKET TERMINAL

PART NO.	FLANGE SIZE	FIGURE	1-9	10-24	25-49	50-99	100+
310-CC-375	.375 SQ.	FIG-E	\$7.25	\$7.00	\$6.75	\$6.25	\$5.75
310-CC-2	2 HOLE	FIG-A	\$7.50	\$7.25	\$7.00	\$6.50	\$6.00
310-CC	.500 SQ.	FIG-D	\$7.25	\$7.00	\$6.75	\$6.25	\$5.75
310-CC-T	.687 SQ.	FIG-C	\$7.95	\$7.50	\$7.25	\$7.00	\$6.75
310-CC-N	1.000 SQ.	FIG-F	\$12.50	\$11.25	\$10.50	\$10.20	\$9.95

312-CC TABULATED SMA PLUG SOCKET TERMINAL

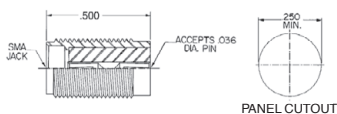
PART NO.	FLANGE SIZE	FIGURE	1-9	10-24	25-49	50-99	100+
312-CC-375	.375 SQ.	FIG-E	\$10.00	\$9.50	\$9.15	\$8.50	\$7.85
312-CC-2	2 HOLE	FIG-B	\$10.25	\$9.75	\$9.40	\$8.75	\$8.10
312-CC	.500 SQ.	FIG-D	\$10.00	\$9.50	\$9.15	\$8.50	\$7.85
312-CC-T	.687 SQ.	FIG-C	\$17.50	\$16.75	\$15.30	\$14.75	\$14.25
312-CC-N	1.000 SQ.	FIG-F	\$21.75	\$20.75	\$20.25	\$20.10	\$19.95

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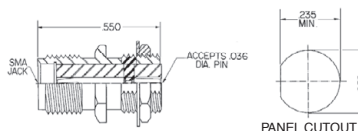
20 21219 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 20

SMA • Bulkhead Mount • Socket Terminal • Captive Contact



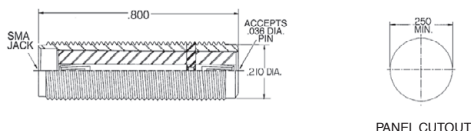
BULKHEAD FEED THROUGH JACK .250 HOLE MOUNT
CAPTIVE CONTACT DOUBLE SOCKET

PART NO	1-9	10-24	25-49	50-99	100+
382-05-02	\$16.00	\$15.45	\$14.70	\$14.30	\$13.40
382-05-02-SF	\$15.50	\$14.95	\$14.20	\$13.80	\$12.90



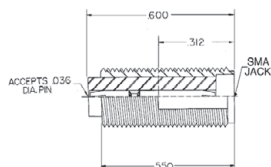
BULKHEAD FEED THROUGH JACK CAPTIVE CONTACT .250
MOUNTING HOLE DOUBLE SOCKET

PART NO	1-9	10-24	25-49	50-99	100+
363-DS	\$18.50	\$18.25	\$16.75	\$15.75	\$15.00
363-DS-SF	\$18.00	\$17.75	\$16.25	\$15.25	\$14.50

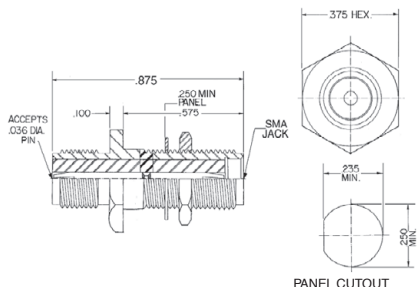


382-02-CC BULKHEAD FEED THROUGH JACK CAPTIVE
CONTACT .250 MOUNTING HOLE DOUBLE SOCKET

PART NO	1-9	10-24	25-49	50-99	100+
382-02-CC	\$18.00	\$16.75	\$16.00	\$15.30	\$14.25
382-02-CC-SF	\$17.50	\$16.25	\$15.50	\$14.80	\$13.75
382-03-CC	\$18.00	\$16.75	\$16.00	\$15.30	\$14.25
382-03-CC-SF	\$17.50	\$16.25	\$15.50	\$14.80	\$13.75

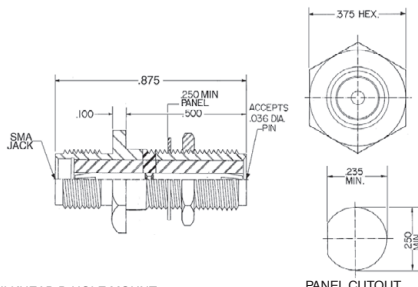


382-03-CC BULKHEAD FEED THROUGH JACK CAPTIVE
CONTACT .250 MOUNTING HOLE WITH .217 DIM.
ACROSS BOTH FLATS DOUBLE SOCKET



BULKHEAD D HOLE MOUNT
SMA JACK TO SOCKET ADAPTER
CAPTIVE CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
364-DS-CC	\$18.50	\$18.25	\$16.75	\$15.75	\$15.00
364-DS-CC-SF	\$18.00	\$17.75	\$16.25	\$15.25	\$14.50



BULKHEAD D HOLE MOUNT
SMA JACK TO SOCKET ADAPTER
CAPTIVE CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
364-1-DS-CC	\$18.50	\$18.25	\$16.75	\$15.75	\$15.00
364-1-DS-CC-SF	\$18.00	\$17.75	\$16.25	\$15.25	\$14.50

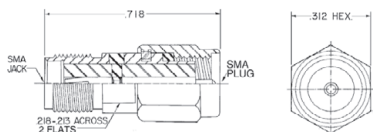
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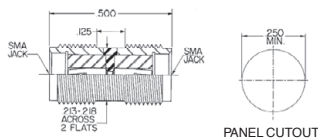
SMA In Series Adapters

★ Operating Frequency DC-26.0 GHz



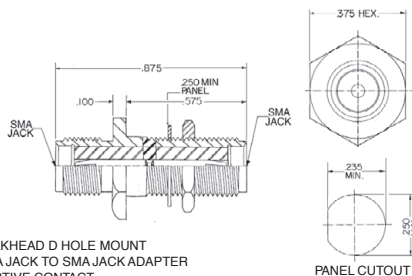
SMA JACK TO SMA PLUG
CAPTIVE CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
357-CC	\$13.25	\$13.00	\$12.25	\$11.75	\$10.75
* 357-CC-26	\$15.25	\$15.00	\$14.25	\$13.75	\$12.75
357-CC-SF	\$12.75	\$12.50	\$11.75	\$11.25	\$10.25
* 357-CC-SF-26	\$14.75	\$14.50	\$13.75	\$13.25	\$12.25



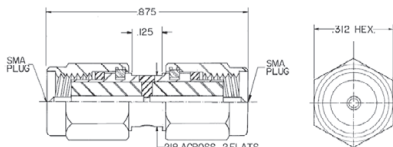
SMA JACK TO SMA JACK ADAPTER
CAPTIVE CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
355-CC	\$13.25	\$13.00	\$12.25	\$11.75	\$10.75
* 355-CC-26	\$15.25	\$15.00	\$14.75	\$14.25	\$13.75
355-CC-SF	\$12.75	\$12.50	\$11.75	\$11.25	\$10.25
* 355-CC-SF-26	\$14.75	\$14.50	\$13.75	\$13.25	\$12.25



BULKHEAD D HOLE MOUNT
SMA JACK TO SMA JACK ADAPTER
CAPTIVE CONTACT

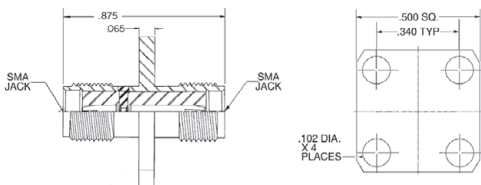
PART NO	1-9	10-24	25-49	50-99	100+
364-CC	\$15.00	\$14.45	\$13.70	\$13.30	\$12.40
* 364-CC-26	\$17.00	\$16.45	\$15.70	\$15.30	\$14.40
364-CC-SF	\$14.50	\$13.95	\$13.20	\$12.80	\$11.90
* 364-CC-SF-26	\$16.50	\$15.95	\$15.20	\$14.80	\$13.90



SMA PLUG TO SMA PLUG
ADAPTER CAPTIVE CONTACT

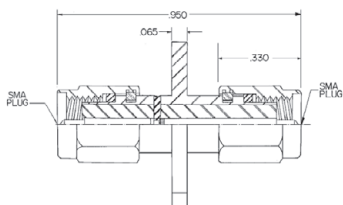
PART NO	1-9	10-24	25-49	50-99	100+
356-CC	\$13.25	\$13.00	\$12.25	\$11.75	\$10.75
* 356-CC-26	\$15.25	\$15.00	\$14.25	\$13.75	\$12.75
356-CC-SF	\$12.75	\$12.50	\$11.75	\$11.25	\$10.25
* 356-CC-SF-26	\$14.75	\$14.50	\$13.75	\$13.25	\$12.25

Operating Frequency DC-18.0 GHz



355-CCFL
SMA FEMALE TO SMA FEMALE
CAPTIVE CONTACT .500 4 HOLE FLANGE

PART NO	1-9	10-24	25-49	50-99	100+
355-CCFL	\$18.00	\$16.75	\$16.00	\$15.30	\$14.00
355-CCFL-SF	\$17.50	\$16.25	\$15.50	\$14.80	\$13.50
356-CCFL	\$29.40	\$28.15	\$27.00	\$26.25	\$25.40
356-CCFL-SF	\$28.90	\$27.65	\$26.50	\$25.75	\$24.90



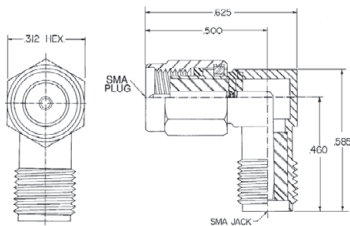
356-CCFL
SMA MALE TO SMA MALE
CAPTIVE CONTACT .500 4 HOLE FLANGE

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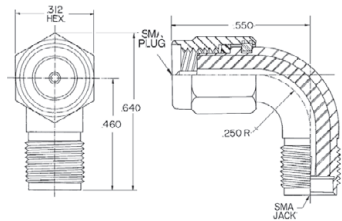
22 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 22

SMA In Series Adapters



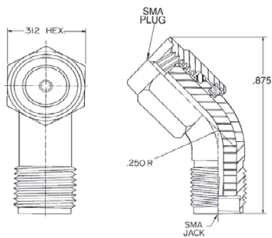
RIGHT ANGLE SMA PLUG TO SMA JACK ADAPTER CAPTIVE CONTACT

PART NO	1-9	10-24	25-49	50-99	100+
357-RA	\$19.75	\$18.50	\$18.00	\$17.50	\$16.00
357-RA-SF	\$18.75	\$17.50	\$17.00	\$16.50	\$15.00



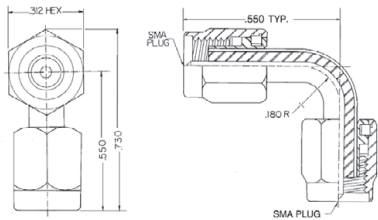
RADIUS RIGHT ANGLE SMA PLUG TO SMA JACK ADAPTER

PART NO	1-9	10-24	25-49	50-99	100+
370	\$29.25	\$27.50	\$26.00	\$24.25	\$23.50
370-26	\$38.50	\$35.25	\$32.50	\$30.00	\$28.25
370-SF	\$28.25	\$26.50	\$25.00	\$23.25	\$22.50
370-SF-26	\$37.50	\$34.25	\$31.50	\$29.00	\$27.25



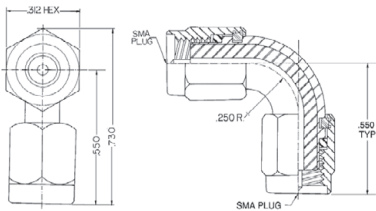
45° ANGLE SMA PLUG TO SMA JACK ADAPTER

PART NO	1-9	10-24	25-49	50-99	100+
370-45	\$43.75	\$40.50	\$38.25	\$35.50	\$30.50
370-45-SF	\$42.75	\$39.50	\$37.25	\$34.50	\$29.50



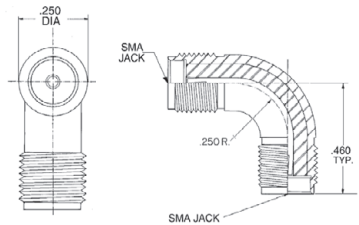
RADIUS RIGHT ANGLE
SMA PLUG TO SMA PLUG ADAPTER 141 SEMI-RIGID TYPE

PART NO	1-9	10-24	25-49	50-99	100+
AA-141-550	\$28.50	\$26.75	\$25.25	\$23.50	\$22.75



RADIUS RIGHT ANGLE SMA PLUG TO SMA PLUG ADAPTER

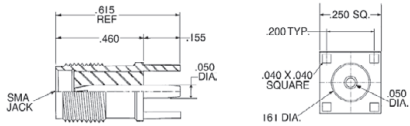
PART NO	1-9	10-24	25-49	50-99	100+
370-M	\$32.75	\$30.50	\$29.25	\$27.50	\$26.25
370-M-SF	\$31.75	\$29.50	\$28.25	\$26.50	\$25.25



RADIUS RIGHT ANGLE SMA JACK TO SMA JACK ADAPTER

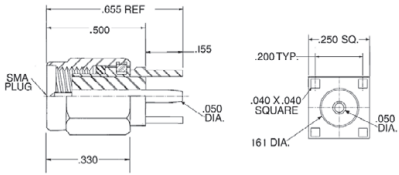
PART NO	1-9	10-24	25-49	50-99	100+
370-F	\$32.75	\$30.50	\$29.25	\$27.50	\$26.25
370-F-SF	\$31.75	\$29.50	\$28.25	\$26.50	\$25.25

SMA PC Mount Receptacles



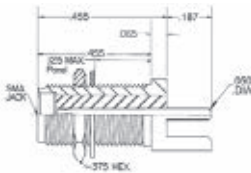
SMA FEMALE PC MOUNT

PART NO	1-9	10-24	25-49	50-99	100+
328PC	\$8.75	\$8.50	\$8.00	\$7.50	\$7.25

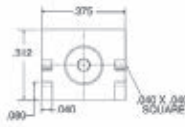


SMA MALE PC MOUNT

PART NO	1-9	10-24	25-49	50-99	100+
329PC	\$10.75	\$10.50	\$10.00	\$9.75	\$9.50

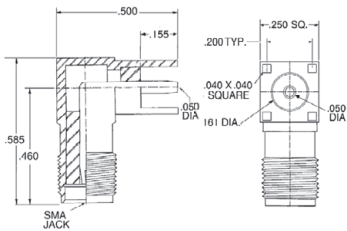


SMA FEMALE LAUNCHER MOUNT



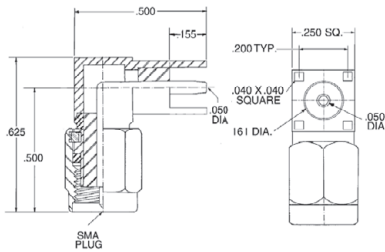
SMA MALE LAUNCHER MOUNT

PART NO	1-9	10-24	25-49	50-99	100+
328PCE	\$9.75	\$9.50	\$9.00	\$8.50	\$8.25
329PCE	\$11.75	\$11.50	\$11.00	\$10.75	\$10.50



SMA FEMALE RIGHT ANGLE PC MOUNT

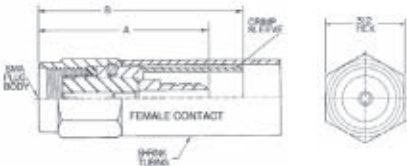
PART NO	1-9	10-24	25-49	50-99	100+
315PC	\$10.75	\$10.50	\$10.00	\$9.50	\$8.75



SMA MALE RIGHT ANGLE PC MOUNT

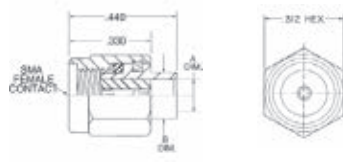
PART NO	1-9	10-24	25-49	50-99	100+
315PCM	\$12.75	\$12.50	\$12.25	\$12.00	\$11.75

Reverse Polarity SMA Connectors Per FCC Part 15.203 Requirement



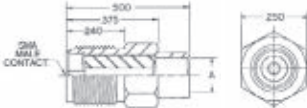
POLARIZED 352 SMA
MALE BODY SMA FEMALE CONTACT FLEXIBLE CABLE

PART NO.	CABLE	A DIM.	B DIM.	1 - 9	10 - 24	25 - 49	50 - 99	100 +
352-1 PZ	RG-55/U, 142, 223	.690	.945	\$8.49	\$7.99	\$7.49	\$6.99	\$6.49
352-2 PZ	RG-58/U, 141, 303, 400	.690	.945	\$8.49	\$7.99	\$7.49	\$6.99	\$6.49
352-3 PZ	RG-174/U, 179, 187, 188, 316	.655	.815	\$8.49	\$7.99	\$7.49	\$6.99	\$6.49



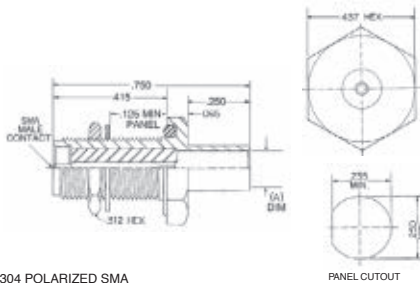
300 & 301 POLARIZED SMA
MALE BODY SMA FEMALE CONTACT SEMI RIGID

PART NO	A DIM	B DIM	CABLE	1-9	10-24	25-49	50-99	100+
300-7 PZ	.143	.187	141	\$5.75	\$5.50	\$5.25	\$5.00	\$4.75
301-1 PZ	.087	.120	085	\$5.75	\$5.50	\$5.25	\$5.00	\$4.75
301-3 PZ	.049	.120	047	\$19.25	\$18.50	\$17.75	\$17.25	\$16.75



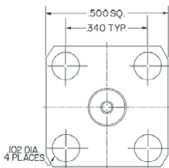
302 POLARIZED SMA
FEMALE BODY MALE CONTACT SEMI RIGID

PART NO	A DIM	CABLE	1-9	10-24	25-49	50-99	100+
302 PZ	.143	.141 SR	\$8.50	\$8.25	\$8.00	\$7.75	\$7.50
302-1 PZ	.0875	.085 SR	\$8.50	\$8.25	\$8.00	\$7.75	\$7.50
302-3 PZ	.049-.052	.047 SR	\$19.25	\$18.50	\$17.75	\$17.25	\$16.75

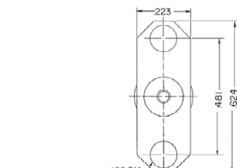
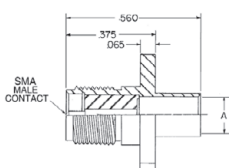


304 POLARIZED SMA
FEMALE BODY SMA MALE CONTACT SEMI RIGID

PART NO	A DIM	CABLE	1-9	10-24	25-49	50-99	100+
304 PZ	.143	.141 SR	\$9.25	\$9.00	\$8.75	\$8.50	\$8.25
304-1 PZ	.0875	.085 SR	\$9.25	\$9.00	\$8.75	\$8.50	\$8.25
304-3 PZ	.049-.052	.047 SR	\$25.50	\$24.50	\$24.25	\$24.00	\$23.25



303 POLARIZED SMA 4 HOLE
FEMALE BODY SMA MALE CONTACT SEMI RIGID



307 POLARIZED SMA 2 HOLE
FEMALE BODY SMA MALE CONTACT SEMI RIGID

PART NO	A DIM	CABLE	1-9	10-24	25-49	50-99	100+
303 PZ	.143	.141	\$10.25	\$10.00	\$9.75	\$9.50	\$9.25
303-1 PZ	.0875	.085	\$10.25	\$10.00	\$9.75	\$9.50	\$9.25
303-2 PZ	.048	.047	\$11.25	\$11.00	\$10.75	\$10.50	\$10.25
307 PZ	.143	.141	\$10.75	\$10.50	\$10.25	\$10.00	\$9.75
307-1 PZ	.0875	.085	\$10.75	\$10.50	\$10.25	\$10.00	\$9.75
307-3 PZ	.048	.047	\$13.75	\$13.50	\$13.25	\$13.00	\$12.75

Reverse Polarity SMA Connectors Per FCC Part 15.203 Requirement

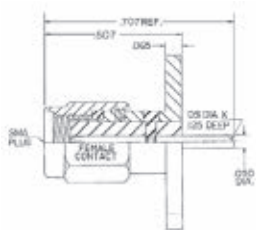


FIG-D

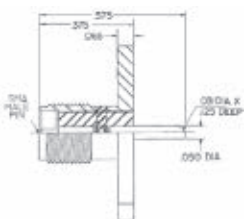


FIG-E

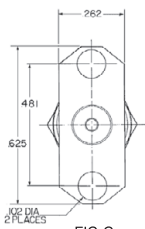


FIG-C

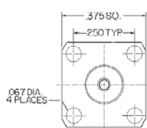


FIG-D

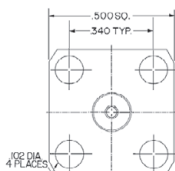


FIG-E

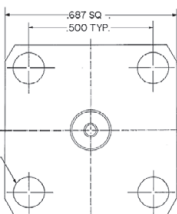


FIG-F

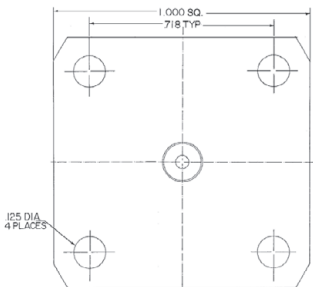
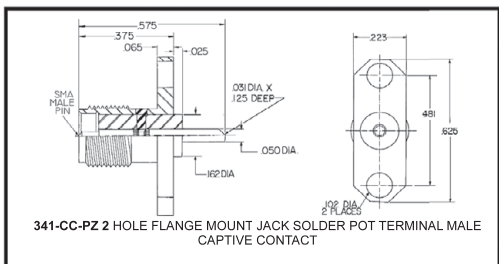


FIG-G



341-CC-PZ 2 HOLE FLANGE MOUNT JACK SOLDER POT TERMINAL MALE CAPTIVE CONTACT

FIG-H

TABULATED, VARIOUS FLANGE MOUNT JACK SOLDER POT TERMINAL CAPTIVE CONTACT

345CC FIG A (SMA PLUG)							
PART NO.	FLANGE SIZE	FIGURE	1-9	10-24	25-49	50-99	100+
345-CC-375-PZ	.375 SQ	FIG D	\$10.50	\$10.05	\$9.50	\$8.95	\$8.35
345-CC-2H-PZ	2 HOLE	FIG C	\$11.25	\$10.80	\$10.25	\$9.75	\$9.25
345-CC-PZ	.500 SQ	FIG E	\$10.50	\$10.05	\$9.50	\$8.95	\$8.35
345-SCC-PZ	.687 SQ	FIG F	\$18.50	\$17.75	\$16.50	\$15.75	\$15.25
345-2CC-PZ	1.000 SQ	FIG G	\$22.75	\$21.75	\$21.25	\$21.10	\$20.95
337CC FIG B (SMA JACK)							
PART NO.	FLANGE SIZE	FIGURE	1-9	10-24	25-49	50-99	100+
337CC-375-PZ	.375 SQ	FIG D	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24
341-CC-PZ	2 HOLE	FIG H	\$6.95	\$6.30	\$5.85	\$5.30	\$4.75
337CC-PZ	.500 SQ	FIG E	\$6.45	\$5.81	\$5.23	\$4.71	\$4.24
320CC-S-PZ	.687 SQ	FIG F	\$7.45	\$6.75	\$6.25	\$5.75	\$5.25
325CC-S-PZ	1.000 SQ	FIG G	\$11.75	\$10.75	\$10.25	\$10.10	\$9.95

For non-captive contact, delete the "CC" designator.
Add the suffix SF for passivated stainless finish.
Suffix BR for brass body with a Hard Nickel Finish.

BR (brass body) unavailable for
ALL SMA MALE (PLUG) CONNECTORS!

**ALL PRICES STATED ARE FOR GOLD
FINISH PLEASE CONSULT FACTORY
FOR BRASS OR STAINLESS FINISH
BODY STYLE**

United Microwave Products Inc.
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TNC Connectors

The TNC series connector was originally designed offering threaded coupling nut mating in lieu of the popular BNC bayonet-type coupling. TNC connectors offer superior electrical performance, higher frequency range the ability to withstand severe shock and vibration requirements.

Using cutting edge microwave technology, United Microwave Products has improved the original TNC connector designs by maintaining minimal disturbance or change in characteristic impedance, reducing tolerance extremes, and using materials such as stainless steel to provide the utmost in mechanical integrity.

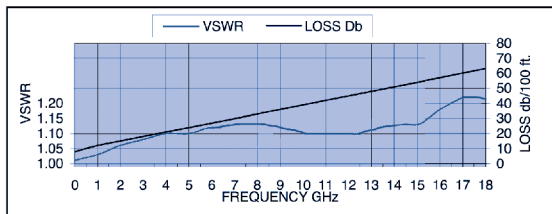
United Microwave TNC connectors are composed of nickel plated brass. However, our TNC connectors are available in passivated stainless steel if desired. Also, they are designed to be free of higher order mode resonance.

All precision TNC connectors will intermate with the MIL-C-39012 interface, conform to Air Force MIL-C-104, ASNAE-68-38A and Navy MIL-T-81490 specifications.

Figure 2.2



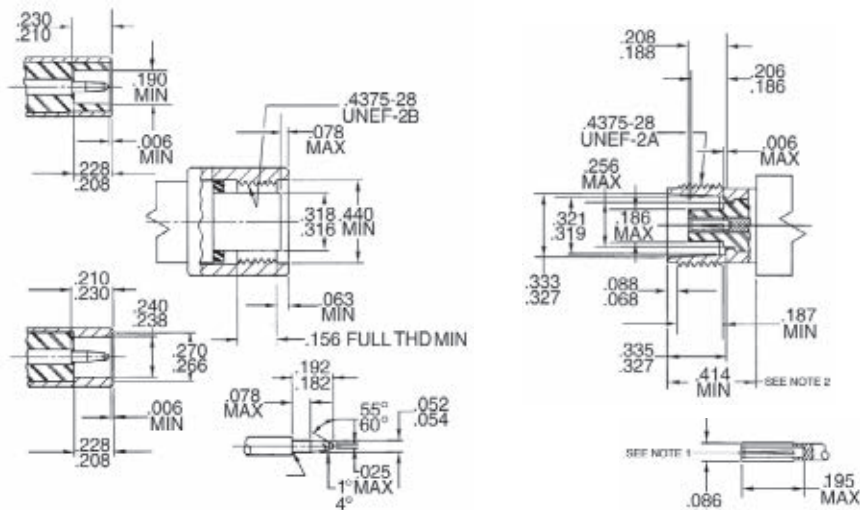
Figure 2.1



GG-165-01.00.0 TNC MALE TO TNC MALE ONE FOOT MICROFLEX 165 CABLE

Figure 2.3

TNC Interface Dimensions Per MIL-C-39012



1. THIS INTERFACE SHALL MEET GAUGE REQUIREMENTS IN MIL-C-39012
2. CLEARANCE FOR MATING CONNECTOR COUPLING NUT

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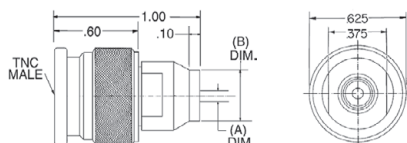
TNC Specifications Per MIL-C-39012

REQUIREMENT	MIL-C-39012 PARA	SPECIFICATIONS																																				
MATERIAL	3.3	Steel corrosion resistant per QQ-S-763, class 303, Beryllium Copper per QQ-C-530 condition HT Silicone Rubber per ZZ-R-765, class II B, Grade 65-75 TFE Fluorocarbon per L-P-403 Soft copper per QQ-B-825																																				
FINISH	3.31	Center contacts: 0.00005 min. gold per MIL-G-45204 type II Grade C over 0.0001 min. copper per MIL-C-14550. Other Metal parts: Sufficient to meet corrosion requirements PARA 3.14 of MIL-C-39012.																																				
DESIGN	3.4	Mating dimensions are in accordance with Figure 2.3																																				
INSULATION RESISTANCE	3.11	10,000 MEGOHMS minimum per MIL-STD-202, Method 302.																																				
DIELECTRIC WITHSTANDING VOLTAGE AND RF HIGH POTENTIAL	3.18	MIL-STD 202, Method 301. <table><tr><th>CABLES</th><th>VRMS @ 60CPS</th><th>VRMS @5MHz</th></tr><tr><td>RG-58, 142, 223, 303, .141 S, R,</td><td>1,500</td><td>1,000</td></tr><tr><td>RG-122, 174, 179, 316 & .085 SR.</td><td>750</td><td>500</td></tr></table>	CABLES	VRMS @ 60CPS	VRMS @5MHz	RG-58, 142, 223, 303, .141 S, R,	1,500	1,000	RG-122, 174, 179, 316 & .085 SR.	750	500																											
CABLES	VRMS @ 60CPS	VRMS @5MHz																																				
RG-58, 142, 223, 303, .141 S, R,	1,500	1,000																																				
RG-122, 174, 179, 316 & .085 SR.	750	500																																				
CONTACT RESISTANCE (Millivolt Drop)	317	<table><tr><th colspan="2">Maximum millivolt drop</th></tr><tr><th>Initial</th><th>After</th></tr><tr><td>Center Contact 1.5</td><td>2.1</td></tr><tr><td>Outer Contact 2.0</td><td>Not applicable</td></tr><tr><td>Braid to Body 0.5</td><td>Not applicable</td></tr></table>	Maximum millivolt drop		Initial	After	Center Contact 1.5	2.1	Outer Contact 2.0	Not applicable	Braid to Body 0.5	Not applicable																										
Maximum millivolt drop																																						
Initial	After																																					
Center Contact 1.5	2.1																																					
Outer Contact 2.0	Not applicable																																					
Braid to Body 0.5	Not applicable																																					
VOLTAGE STANDING WAVE RATIO (VSWR)	3.14	<table><tr><th colspan="3">Straight Plugs and Jacks</th></tr><tr><th>CABLES</th><th colspan="2">VSWR</th></tr><tr><td>RG- 122, 174, 179 & 316</td><td>1.15±0.02</td><td>(F) GHz</td></tr><tr><td>RG-58, 142, 223 & 303</td><td>1.15±0.01</td><td>(F) GHz</td></tr><tr><td>.085 DIA. S.R. (RG-405)</td><td>1.15±0.01</td><td>(F) GHz</td></tr><tr><td>.141 DIA. S.R. (RG-402)</td><td>1.05±0.005</td><td>(F) GHz</td></tr><tr><th colspan="3">Right Angle Plugs and Jacks</th></tr><tr><th>CABLES</th><th colspan="2">VSWR</th></tr><tr><td>RG- 122, 174, 179 & 316</td><td>1.15±0.03</td><td>(F) GHz</td></tr><tr><td>RG-58, 142, 223 & 303</td><td>1.15±0.02</td><td>(F) GHz</td></tr><tr><td>.085 DIA. S.R. (RG-405)</td><td>1.15±0.015</td><td>(F) GHz</td></tr><tr><td>.141 DIA. S.R. (RG-402)</td><td>1.05±0.01</td><td>(F) GHz</td></tr></table>	Straight Plugs and Jacks			CABLES	VSWR		RG- 122, 174, 179 & 316	1.15±0.02	(F) GHz	RG-58, 142, 223 & 303	1.15±0.01	(F) GHz	.085 DIA. S.R. (RG-405)	1.15±0.01	(F) GHz	.141 DIA. S.R. (RG-402)	1.05±0.005	(F) GHz	Right Angle Plugs and Jacks			CABLES	VSWR		RG- 122, 174, 179 & 316	1.15±0.03	(F) GHz	RG-58, 142, 223 & 303	1.15±0.02	(F) GHz	.085 DIA. S.R. (RG-405)	1.15±0.015	(F) GHz	.141 DIA. S.R. (RG-402)	1.05±0.01	(F) GHz
Straight Plugs and Jacks																																						
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.085 DIA. S.R. (RG-405)	1.15±0.015	(F) GHz																																				
.141 DIA. S.R. (RG-402)	1.05±0.01	(F) GHz																																				
INSERTION LOSS	3.29	Straight plugs and jacks, dB Max. = .05 x√GHz Freq. Right Angle plugs, dB Max. = .15x√GHz Freq.																																				
FORCE TO ENGAGE AND DISENGAGE	3.51	Longitudinal force is not applicable. torque 2 in-lbs. maximum.																																				
COUPLING NUT PROOF TORQUE	3.27	30 inch-pounds minimum.																																				

TNC Specifications Per MIL-C-39012

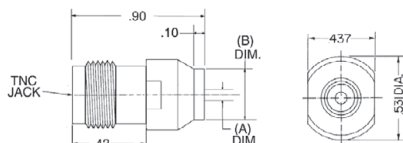
REQUIREMENT	MIL C 39012 PARA	SPECIFICATIONS			
CONNECTOR DURABILITY	3.16	Insertion and withdrawal 500 cycles minimum. Maximum rate of 12 Cycles Per Minute. Connector shall show no evidence of mechanical failure and shall meet the mating characteristics requirements of MIL-C-39012,PARA 3.26			
CABLE RETENTION FORCE	3.26	See Table I			
	TABLE 1 -Cable retention force.				
	Cable dielectric Outer diameter	Non crimp Single braid	Crimp Single braid		
	Inches (max)	Center contact		Center contact	
		Captive Pounds (max)	Non Captive Pounds (max)	Captive Pounds (max)	Non Captive Pounds (max)
	.066	25	20	25	20
	.110	35	30	35	30
	.122	45	40	45	40
MATING CHARACTERISTICS	3.7	Contacts with spring members Center contact (female) Oversize test pin - .055 minimum diameter Test pin finish - 16/ Insertion depth - .1250 Number of insertions - 1 Insertion force test: Steel test pin Diameter - .0540 minimum Insertion depth - .1250 Test pin finish - 16/ Insertion force - 2 lbs. maximum Withdrawal force test: Steel test pin Diameter - .052 maximum Insertion depth - .1250 Withdrawal force - 2 Ounce minimum Test pin finish - 16/			
VIBRATION	3.18	MIL-STD-202, method 204, test condition B. No discontinuities.			
SHOCK	3.19	MIL-STD-202, method 213, test condition I. No discontinuities.			
THERMAL SHOCK	3.20	Refer to applicable military slash sheet or consult factory.			
CORROSION SALT SPRAY	3.13	MIL-STD-202, method 101, test condition B, the salt solution shall be 5 percent.			
MOISTURE RESISTANCE	3.23	MIL-STD-202, method 106. Insulation 200 MEGOHMS min. within 5 minutes after removal from humidity.			
CABLE RETENTION	3.24	Refer to applicable military slash sheet or consult factory.			
CORONA LEVEL	3.22	Refer to applicable military slash sheet or consult factory.			

TNC Connectors to Semi Rigid Cables



TNC STRAIGHT CABLE PLUG DIRECT SOLDER

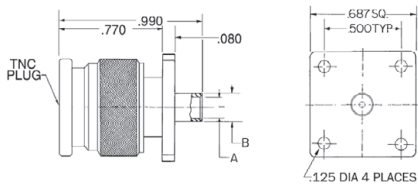
PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
516-087	RG-405	.089	.12	\$17.50	\$16.00	\$15.25	\$14.50	\$13.75
516-141	RG-402	.145	.18	\$17.50	\$16.00	\$15.25	\$14.50	\$13.75



TNC STRAIGHT CABLE JACK DIRECT SOLDER

PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
517-087	RG-405	.089	.12	\$18.50	\$17.00	\$16.25	\$15.50	\$14.75
517-141	RG-402	.145	.18	\$18.50	\$17.00	\$16.25	\$15.50	\$14.75

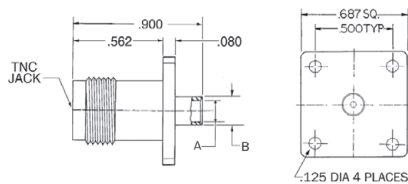
FLANGE MOUNT ALSO AVAIL WITH #3-56
THREADS CONTACT FACTORY FOR DETAILS



TNC 4 HOLE CABLE JACK DIRECT SOLDER

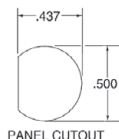
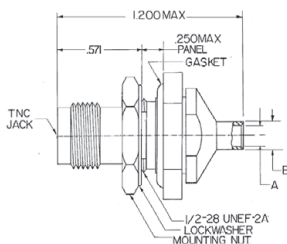
PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
530M-087	RG-405	.089	.12	\$34.00	\$32.00	\$31.00	\$29.00	\$26.00
530M-141	RG-402	.145	.18	\$34.00	\$32.00	\$31.00	\$29.00	\$26.00

FLANGE MOUNT ALSO AVAIL WITH #3-56
THREADS CONTACT FACTORY FOR DETAILS



TNC 4 HOLE FLANGE STRAIGHT CABLE JACK DIRECT SOLDER

PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
530-1	RG-405	.089	.12	\$24.75	\$22.50	\$21.25	\$19.00	\$17.50
530-2	RG-402	.145	.18	\$24.75	\$22.50	\$21.25	\$19.00	\$17.50



TNC BULKHEAD FEED THROUGH CABLE JACK DIRECT SOLDER

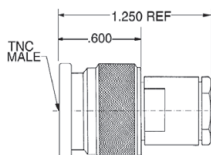
PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
531-1	RG-405	.089	.12	\$19.50	\$18.00	\$17.00	\$15.50	\$14.00
531-2	RG-402	.145	.18	\$19.50	\$18.00	\$17.00	\$15.50	\$14.00
531-1SF (STAINLESS BODY)	RG-405	.089	.12	\$39.00	\$37.50	\$36.00	\$34.00	\$31.50
531-2SF (STAINLESS BODY)	RG-402	.145	.18	\$39.00	\$37.50	\$36.00	\$34.00	\$31.50

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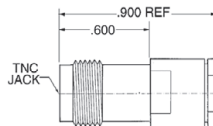
30 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 30

TNC Connectors Solder Crimp Clamp



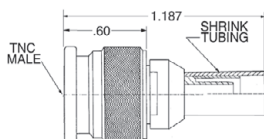
TNC STRAIGHT CABLE PLUG CLAMP

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
528-1 CLP	RG-188, 316	\$12.50	\$12.25	\$11.50	\$11.00	\$10.50
528-2 CLP	RG-55, 58, 141, 142, 223, 303	\$12.50	\$12.25	\$11.50	\$11.00	\$10.50



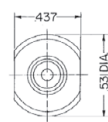
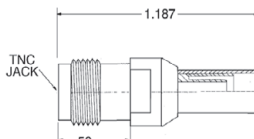
TNC STRAIGHT CABLE JACK CLAMP

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
529-1 CLP	RG-188, 316	\$21.50	\$20.25	\$19.50	\$18.75	\$18.00
529-2 CLP	RG-55, 58, 141, 142, 223, 303	\$21.50	\$20.25	\$19.50	\$18.75	\$18.00



TNC STRAIGHT CABLE PLUG SOLDER/CRIMP

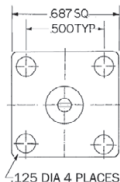
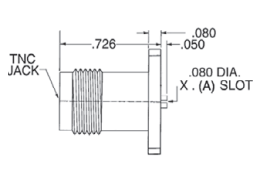
PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
528-1	RG-188, 316	\$14.50	\$14.25	\$13.50	\$13.00	\$12.50
528-2	RG-55, 58, 141, 142, 223, 303	\$14.50	\$14.25	\$13.50	\$13.00	\$12.50



TNC STRAIGHT CABLE JACK SOLDER/CRIMP

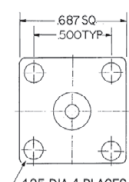
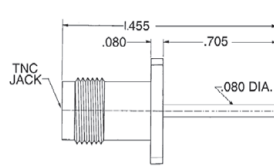
PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
529-1	RG-188, 316	\$21.50	\$20.25	\$19.50	\$18.75	\$18.00
529-3	RG-55, 58, 142, 223, 303, 400	\$21.50	\$20.25	\$19.50	\$18.75	\$18.00

TNC Panel Mount Receptacles



TNC JACK FLANGE MOUNT RECEPTACLE SLOT

PART NO.	SLOT WITH	1-9	10-24	25-49	50-99	100+
562-1	.012	\$12.45	\$11.75	\$10.50	\$9.75	\$9.10
562-2	.018	\$12.45	\$11.75	\$10.50	\$9.75	\$9.10
562-3	.028	\$12.45	\$11.75	\$10.50	\$9.75	\$9.10



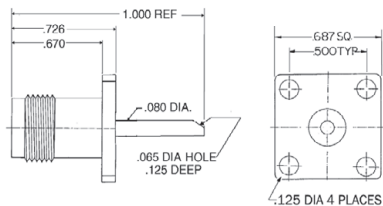
TNC JACK FLANGE MOUNT RECEPTACLE

PART NO.	1-9	10-24	25-49	50-99	100+
527S	\$12.45	\$11.75	\$10.50	\$9.75	\$9.10

United Microwave Products Inc.

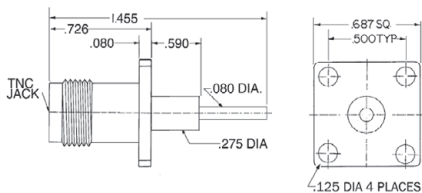
Direct Sales, Tech Support and Current Order Status

TNC Panel Mount Receptacles



TNC JACK FLANGE MOUNT RECEPTACLE SOLDER POT

PART NO.	1-9	10-24	25-49	50-99	100+
532	\$12.45	\$11.75	\$10.50	\$9.75	\$9.10

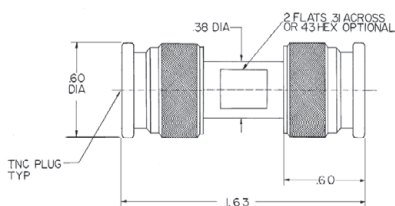


TNC JACK FLANGE MOUNT RECEPTACLE EXTENDED INSULATOR & TERMINAL

PART NO.	1-9	10-24	25-49	50-99	100+
513	\$12.45	\$11.75	\$10.50	\$9.75	\$9.10

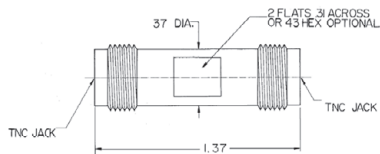
TNC In Series Adapters

These Precision Adapters are Furnished With Stainless Steel Bodies Operating Range DC-18GHz



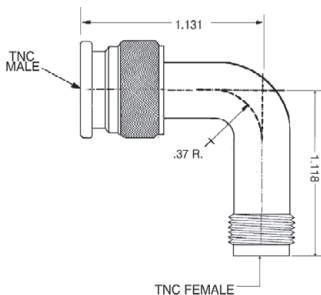
TNC PLUG TO TNC PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
1830	\$36.50	\$34.50	\$33.00	\$31.00	\$28.00



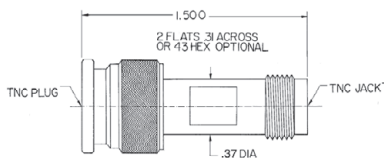
TNC JACK TO TNC JACK

PART NO.	1-9	10-24	25-49	50-99	100+
1810	\$36.50	\$34.50	\$33.00	\$31.00	\$28.00



TNC PLUG TO TNC JACK RADIUS RIGHT ANGLE

PART NO.	1-9	10-24	25-49	50-99	100+
6421	\$115.45	\$106.00	\$98.00	\$92.00	\$85.00



TNC JACK TO TNC PLUG CONNECTOR SAVER

PART NO.	1-9	10-24	25-49	50-99	100+
1820	\$36.50	\$34.50	\$33.00	\$31.00	\$28.00

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32 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 32

Type "N" Connectors

The type N series coaxial connectors were originally designed as medium-size low voltage constant impedance 50 OHM connectors. Type N connectors found immediate popularity for microwave applications because of the 7 mm size air-filled mating interface. United Microwave Products has developed a complete line of precision type N series connectors. Constructed of stainless steel, Teflon dielectrics, and gold plated beryllium copper center contacts, these precision N connectors will mate nondestructively to the standard MIL-C-39012 interface.

Additionally, United Microwave Products has extended the upper operating frequency to 18.0 GHz as compared to 11.0 GHz offered in MIL-C-39012. These precision type N connectors are offered for both semi-rigid and flexible cables, panel mount receptacles, in-series adapters, and strip-line transmission applications. Panel mount N connectors are available in both nickel plated brass & passivated stainless steel.



Figure 3.1

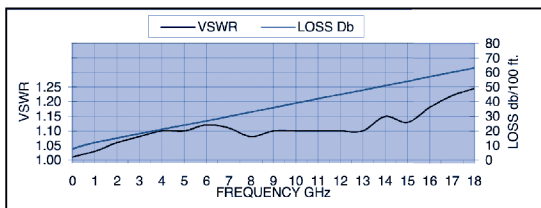
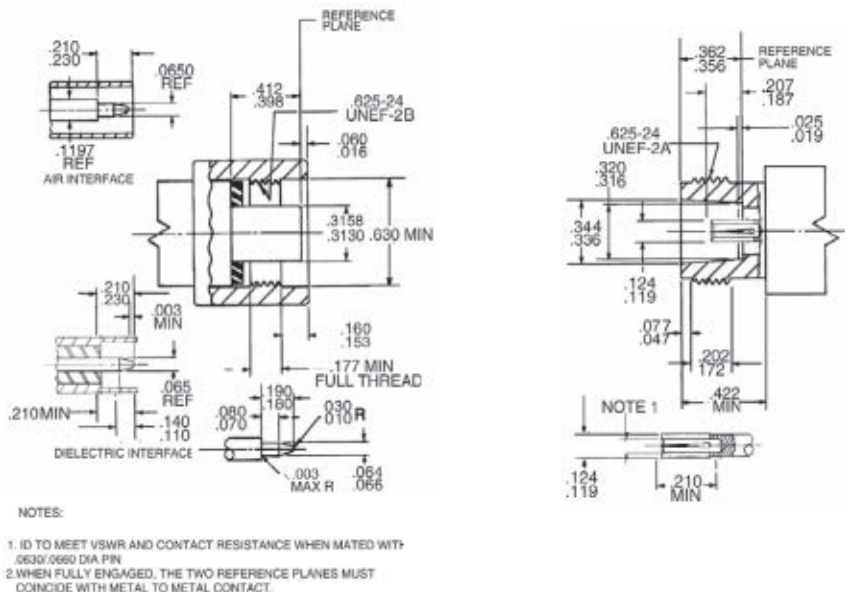


Figure 3.2 OO-165 -01.00.0 "N" MALE to "N" MALE ONE FOOT MICROFLEX 165 CABLE

Figure 3.3

Type "N" Interface Dimensions



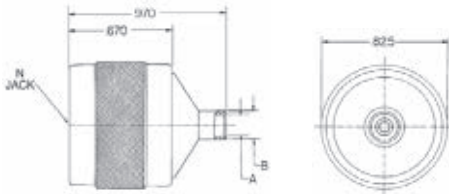
N Specifications Per MIL-C-39012

REQUIREMENT	MIL-C-39012 PARA	SPECIFICATIONS																						
MATERIAL	3.3	Steel corrosion resistant per QQ-S-763, class 303, Beryllium Copper per QQ-C-530 condition HT Silicone Rubber per ZZ-R-765, class II B, Grade 65-75 TFE Fluorocarbon per L-P-403 Soft copper per QQ-B-825																						
FINISH	3.31	Center contacts: 0.00005 min. gold per MIL-G-45204 type II Grade C over 0.0001 min. copper per MIL-C-14550. Other Metal parts: Sufficient to meet corrosion requirements PARA 3.14 of MIL-C-39012.																						
DESIGN	3.4	Mating dimensions are in accordance with page 33 Figure 3.3 of this catalog																						
INSULATION RESISTANCE	3.11	10,000 MEGOHMS minimum per MIL-STD-202, Method 302.																						
DIELECTRIC WITHSTANDING VOLTAGE AND RF HIGH POTENTIAL	3.18	MIL-STD 202, Method 301. <table><thead><tr><th>CABLES</th><th>VRMS @ 60CPS</th><th>VRMS @5MHz</th></tr></thead><tbody><tr><td>RG-214, 225 & 393</td><td>2500</td><td>1500</td></tr><tr><td>RG-58, 142, 223, 303 & .141 S.R.</td><td>1,500</td><td>1000</td></tr><tr><td>RG-122, 174, 179, 316 & .085 S.R.</td><td>750</td><td>500</td></tr></tbody></table>	CABLES	VRMS @ 60CPS	VRMS @5MHz	RG-214, 225 & 393	2500	1500	RG-58, 142, 223, 303 & .141 S.R.	1,500	1000	RG-122, 174, 179, 316 & .085 S.R.	750	500										
CABLES	VRMS @ 60CPS	VRMS @5MHz																						
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RG-122, 174, 179, 316 & .085 S.R.	750	500																						
CONTACT RESISTANCE (Millivolt Drop)	3.17	Maximum millivolt drop <table><thead><tr><th>Initial</th><th>After</th></tr></thead><tbody><tr><td>Center Contact 1.5</td><td>2.5</td></tr><tr><td>Outer Contact 2.0</td><td>Not applicable</td></tr><tr><td>Braid to Body 0.5</td><td>Not applicable</td></tr></tbody></table>	Initial	After	Center Contact 1.5	2.5	Outer Contact 2.0	Not applicable	Braid to Body 0.5	Not applicable														
Initial	After																							
Center Contact 1.5	2.5																							
Outer Contact 2.0	Not applicable																							
Braid to Body 0.5	Not applicable																							
VOLTAGE STANDING WAVE RATIO (VSWR)	3.14	Straight Plugs and Jacks <table><thead><tr><th>CABLES</th><th>VSWR</th></tr></thead><tbody><tr><td>RG-214, 225 & 393</td><td>1.20+ .025 (F) GHz</td></tr><tr><td>RG- 122, 174, 179 & 316</td><td>1.15+0.02 (F) GHz</td></tr><tr><td>RG-58, 142, 223 & 303</td><td>1.15+0.01 (F) GHz</td></tr><tr><td>.085 DIA. S.R. (RG-405)</td><td>1.15+0.01 (F) GHz</td></tr><tr><td>.141 DIA. S.R. (RG-402)</td><td>1 .05+0.005 (F) GHz</td></tr></tbody></table> Right Angle Plugs and Jacks <table><tbody><tr><td>RG- 214, 225 & 393</td><td>1.20+0.03 (F) GHz</td></tr><tr><td>RG- 122, 174, 179 & 316</td><td>1.15+0.03 (F) GHz</td></tr><tr><td>RG-58, 142, 223 & 303</td><td>1.15+0.02 (F) GHz</td></tr><tr><td>.085 DIA. S.R. (RG-405)</td><td>1.15+0.015 (F) GHz</td></tr><tr><td>.141 DIA. S.R. (RG-402)</td><td>1 .05+0.01 (F) GHz</td></tr></tbody></table>	CABLES	VSWR	RG-214, 225 & 393	1.20+ .025 (F) GHz	RG- 122, 174, 179 & 316	1.15+0.02 (F) GHz	RG-58, 142, 223 & 303	1.15+0.01 (F) GHz	.085 DIA. S.R. (RG-405)	1.15+0.01 (F) GHz	.141 DIA. S.R. (RG-402)	1 .05+0.005 (F) GHz	RG- 214, 225 & 393	1.20+0.03 (F) GHz	RG- 122, 174, 179 & 316	1.15+0.03 (F) GHz	RG-58, 142, 223 & 303	1.15+0.02 (F) GHz	.085 DIA. S.R. (RG-405)	1.15+0.015 (F) GHz	.141 DIA. S.R. (RG-402)	1 .05+0.01 (F) GHz
CABLES	VSWR																							
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RG-58, 142, 223 & 303	1.15+0.02 (F) GHz																							
.085 DIA. S.R. (RG-405)	1.15+0.015 (F) GHz																							
.141 DIA. S.R. (RG-402)	1 .05+0.01 (F) GHz																							
INSERTION LOSS	3.29	Straight plugs and jacks, dB Max. = .05 x/GHz Freq. Right Angle plugs, dB Max. = .15x/GHz Freq.																						
FORCE TO ENGAGE AND DISENGAGE	3.51	Longitudinal force is not applicable. torque 2 in-lbs. maximum.																						
COUPLING NUT PROOF TORQUE	3.6	30 inch-pounds minimum.																						

N Specifications Per MIL-C-39012

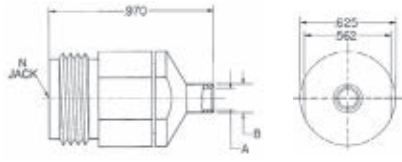
REQUIREMENT	MIL C 39012 PARA	SPECIFICATIONS																																			
CONNECTOR DURABILITY	3.16	Insertion and withdrawal 500 cycles minimum. Maximum rate of 12 Cycles Per Minute. Connector shall show no evidence of mechanical failure and shall meet the mating characteristics requirements of MIL-C-39012,PARA 3.26																																			
CABLE RETENTION FORCE	3.26	See Table I TABLE 1 -Cable retention force. <table><tr><td>Cable dielectric Outer diameter</td><td colspan="2">Non crimp Single braid</td><td colspan="2">Crimp Single braid</td></tr><tr><td></td><td colspan="2">Center contact</td><td colspan="2">Center contact</td></tr><tr><td>Inches (max)</td><td>Captive Pounds (max)</td><td>Non Captive Pounds (max)</td><td>Captive Pounds (max)</td><td>Non Captive Pounds (max)</td></tr><tr><td>.036</td><td>13</td><td>10</td><td>13</td><td>10</td></tr><tr><td>.066</td><td>25</td><td>20</td><td>25</td><td>20</td></tr><tr><td>.110</td><td>35</td><td>30</td><td>35</td><td>30</td></tr><tr><td>.122</td><td></td><td>40</td><td>45</td><td>40</td></tr></table>	Cable dielectric Outer diameter	Non crimp Single braid		Crimp Single braid			Center contact		Center contact		Inches (max)	Captive Pounds (max)	Non Captive Pounds (max)	Captive Pounds (max)	Non Captive Pounds (max)	.036	13	10	13	10	.066	25	20	25	20	.110	35	30	35	30	.122		40	45	40
Cable dielectric Outer diameter	Non crimp Single braid		Crimp Single braid																																		
	Center contact		Center contact																																		
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.066	25	20	25	20																																	
.110	35	30	35	30																																	
.122		40	45	40																																	
MATING CHARACTERISTICS	3.7	Contacts with spring members Center contact (female) Oversize test pin - .0670 inch minimum diameter Test pin finish - 16/ Insertion depth - .1250 inch Number of insertions - 3 Insertion force test: Steel test pin Diameter - .065 minimum diameter Insertion depth - .1250 inch Test pin finish - 16/ Insertion force - 3 pounds maximum Withdrawal force test: Steel test pin Diameter - .064 maximum diameter Insertion depth - .1250 Withdrawal force - 1 Ounce minimum Test pin finish - 16/																																			
VIBRATION	3.18	MIL-STD-202, method 204, test condition B. No discontinuities.																																			
SHOCK	3.19	MIL-STD-202, method 213, test condition I. No discontinuities.																																			
THERMAL SHOCK	3.20	Refer to applicable military slash sheet or consult factory.																																			
CORROSION SALT SPRAY	3.13	MIL-STD-202, method 101, test condition B , the salt solution shall be 5 percent.																																			
MOISTURE RESISTANCE	3.23	MIL-STD-202, method 106. Insulation 200 MEGOHMS min. within 5 minutes after removal from humidity.																																			
CABLE RETENTION	3.24	Refer to applicable military slash sheet or consult factory.																																			
CORONA LEVEL	3.22	Refer to applicable military slash sheet or consult factory.																																			

"N" Connectors to Semi Rigid Cables



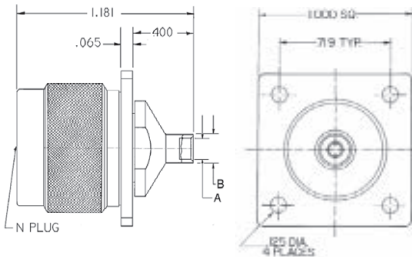
N PLUG STRAIGHT CABLE DIRECT SOLDER

PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
1523-1	RG-402	.145	.18	\$12.50	\$11.75	\$10.75	\$9.75	\$9.50
1523-1SF	RG-402	.145	.18	\$15.50	\$14.75	\$13.75	\$12.75	\$12.50
1523-2	RG-405	.089	.12	\$12.50	\$11.75	\$10.75	\$9.75	\$9.50
1523-2SF	RG-405	.089	.12	\$15.50	\$14.75	\$13.75	\$12.75	\$12.50



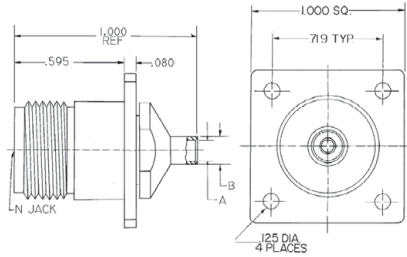
N JACK STRAIGHT CABLE DIRECT SOLDER

PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
1519-1	RG-402	.145	.18	\$17.50	\$16.75	\$16.25	\$15.75	\$14.50
1519-2	RG-405	.089	.12	\$17.50	\$16.75	\$16.25	\$15.75	\$14.50



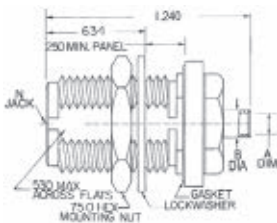
N 4 HOLE FLANGE STRAIGHT CABLE PLUG DIRECT SOLDER

PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
1523-1FLG	RG-402	.145	.18	\$42.50	\$41.75	\$40.50	\$37.25	\$34.75
1523-2FLG	RG-405	.089	.12	\$42.50	\$41.75	\$40.50	\$37.25	\$34.75



N 4 HOLE FLANGE STRAIGHT CABLE JACK DIRECT SOLDER

PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
1524-1	RG-402	.145	.18	\$37.50	\$36.75	\$35.50	\$32.25	\$29.75
1524-2	RG-405	.089	.12	\$37.50	\$36.75	\$35.50	\$32.25	\$29.75



N BULKHEAD FEED THROUGH JACK SEMI-RIGID FLEXIBLE CABLE RG-TYPE

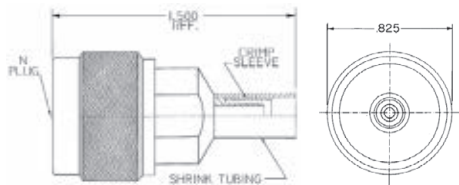
PART NO.	CABLE	(A) DIM	(B) DIM	1-9	10-24	25-49	50-99	100+
1526-1	RG-402	.145	.18	\$19.50	\$18.75	\$17.75	\$16.50	\$15.50
1526-2	RG-405	.089	.12	\$19.50	\$18.75	\$17.75	\$16.50	\$15.50
1526-3	RG-401	.255	.30	\$19.50	\$18.75	\$17.75	\$16.50	\$15.50
1526-HEL	1/4 HELIAX	.255	.30	\$23.50	\$22.75	\$21.75	\$20.50	\$19.50
1526-LL	1/4 LOW LOSS	.255	.30	\$23.50	\$22.75	\$21.75	\$20.50	\$19.50

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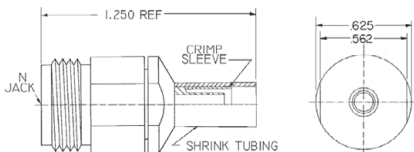
Prices listed effective as of 1 July 2008 and subject to change at any time.

"N" Connectors to Flexible Cables



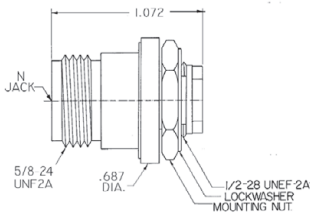
N PLUG SOLDER/CRIMP RG TYPE FLEXIBLE CABLE

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
1523-1FLX	RG-155, 142, 223	\$17.50	\$16.75	\$15.55	\$14.75	\$14.25
1523-2FLX	RG- 58, 141, 303	\$17.50	\$16.75	\$15.55	\$14.75	\$14.25
1523-3FLX	RG-304	\$17.50	\$16.75	\$15.55	\$14.75	\$14.25



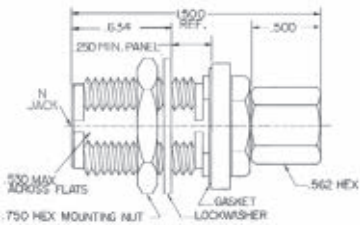
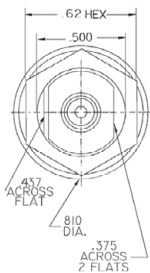
N JACK SOLDER/CRIMP RG TYPE FLEXIBLE CABLE

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
1519-1FLX	RG-155, 142, 223	\$18.75	\$17.50	\$16.75	\$15.50	\$14.75
1519-2FLX	RG- 58, 141, 303	\$18.75	\$17.50	\$16.75	\$15.50	\$14.75
1519-3FLX	RG-304	\$18.75	\$17.50	\$16.75	\$15.50	\$14.75



N JACK BULKHEAD FEEDTHROUGH SOLDER/CRIMP RG TYPE FLEXIBLE CABLE

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
1519-1CLP	RG-155, 142, 223	\$48.75	\$44.50	\$41.25	\$39.70	\$37.50
1519-2CLP	RG- 58, 141, 303	\$48.75	\$44.50	\$41.25	\$39.70	\$37.50
1519-3CLP	RG-304	\$48.75	\$44.50	\$41.25	\$39.70	\$37.50



N JACK BULKHEAD FEEDTHROUGH SOLDER/CRIMP RG TYPE FLEXIBLE CABLE

PART NO.	CABLE	1-9	10-24	25-49	50-99	100+
1526-1FLX	RG-155, 142, 223	\$29.50	\$29.25	\$28.75	\$27.50	\$27.25
1526-2FLX	RG- 58, 141, 303	\$29.50	\$29.25	\$28.75	\$27.50	\$27.25
1526-3FLX	RG-304	\$29.50	\$29.25	\$28.75	\$27.50	\$27.25

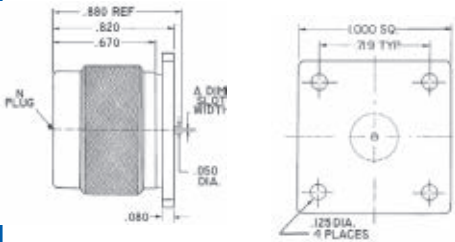


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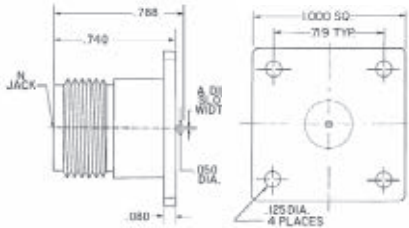
37 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 37

"N" Panel Mount Receptacles



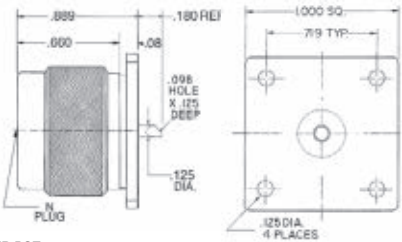
SLOT CAPTIVE CONTACT PLUG TERMINAL FLANGE MOUNT

PART NO.	SLOT WITH	1-9	10-24	25-49	50-99	100+
1549-1	.012	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50
1549-2	.018	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50
1549-3	.028	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50



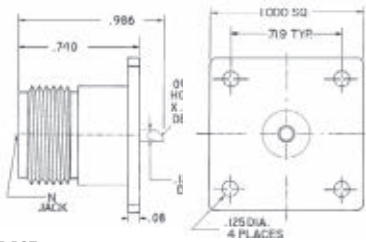
SLOT CAPTIVE CONTACT JACK TERMINAL FLANGE MOUNT

PART NO.	SLOT WITH	1-9	10-24	25-49	50-99	100+
1552-1	.012	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25
1552-2	.018	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25
1552-3	.028	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25



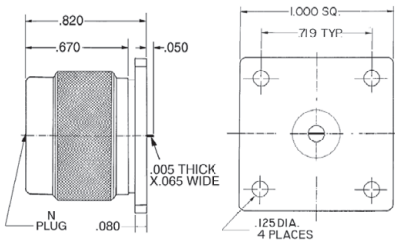
SOLDER POT
FLANGE MOUNT PLUG
CAPTIVE CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
1543	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50



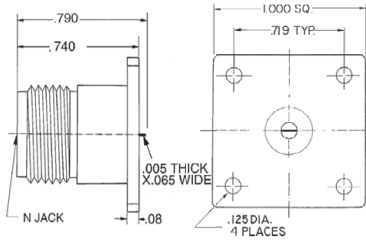
SOLDER POT
FLANGE MOUNT JACK
CAPTIVE CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
1544	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25



STRIPLINE
FLANGE MOUNT PLUG
CAPTIVE CONTACT

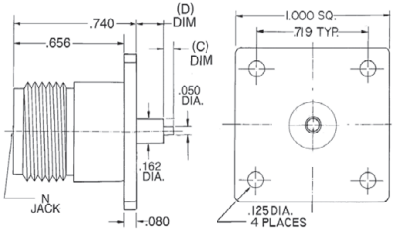
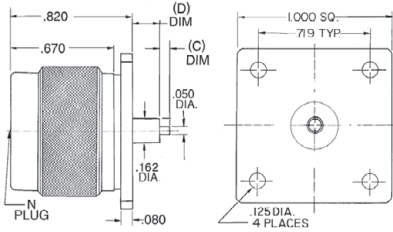
PART NO.	1-9	10-24	25-49	50-99	100+
1539	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50



STRIPLINE
FLANGE MOUNT JACK
CAPTIVE CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
1538	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25

"N" Panel Mount Receptacles



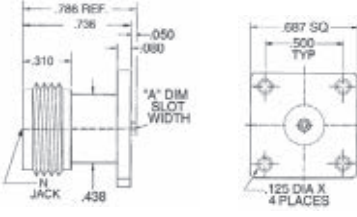
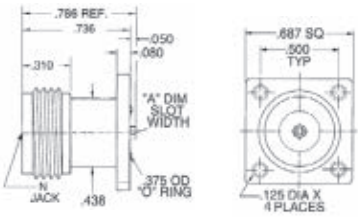
EXTENDED TERMINAL FLANGE MOUNT PLUG CAPTIVE CONTACT

PART NO.	(C) DIM	(D) DIM	1-9	10-24	25-49	50-99	100+
1545-550	.160	.550	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50
1545-375	.050	.375	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50
1545-260	.200	.260	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50
1545-380	.050	.380	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50
1545-320	.055	.320	\$19.75	\$18.95	\$17.50	\$16.50	\$15.50

EXTENDED TERMINAL FLANGE MOUNT JACK CAPTIVE CONTACT

PART NO.	(C) DIM	(D) DIM	1-9	10-24	25-49	50-99	100+
1540-550	.160	.550	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25
1540-375	.050	.375	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25
1540-260	.200	.260	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25
1540-380	.050	.380	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25
1540-320	.055	.320	\$14.75	\$13.50	\$12.75	\$11.75	\$10.25

"N" Panel Mount Receptacles TNC Flange

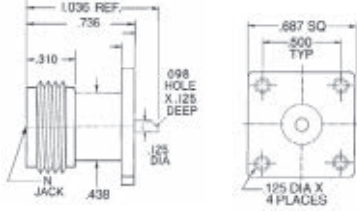
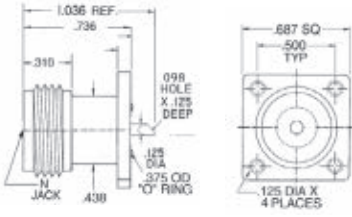


SLOT TERMINAL TNC FLANGE JACK O-RING CAPTIVE CONTACT

PART NO.	SLOT WITH	1-9	10-24	25-49	50-99	100+
1552-1 687 O	.012	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75
1552-2 687 O	.015	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75
1552-3 687 O	.018	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75

SLOT TERMINAL TNC FLANGE JACK CAPTIVE CONTACT

PART NO.	SLOT WITH	1-9	10-24	25-49	50-99	100+
1552-1 687	.012	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25
1552-2 687	.015	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25
1552-3 687	.018	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25



SOLDER POT JACK TNC FLANGE MOUNT O RING CAPTIVE CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
1544-687 O	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75

SOLDER POT TNC FLANGE MOUNT JACK CAPTIVE CONTACT

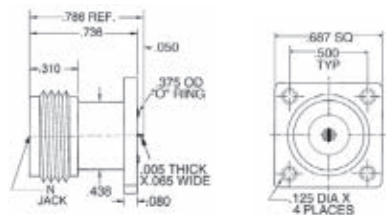
PART NO.	1-9	10-24	25-49	50-99	100+
1544-687	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25

United Microwave Products Inc.

Direct Sales, Tech Support and Current Order Status

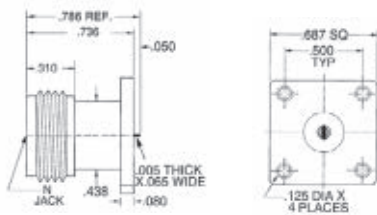
39 12229 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 39

"N" Panel Mount Receptacles TNC Flange



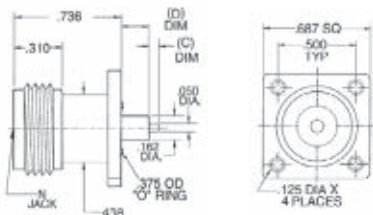
STRIPLINE TNC O RING FLANGE MOUNT JACK CAPTIVE CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
1538-687 O	\$16.75	\$16.10	\$15.50	\$14.50	\$13.25



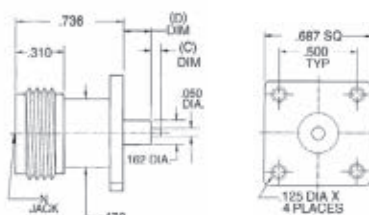
STRIPLINE TNC FLANGE MOUNT JACK CAPTIVE CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
1538-687	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25



EXTENDED TNC TERMINAL O RING FLANGE JACK CAPTIVE CONTACT

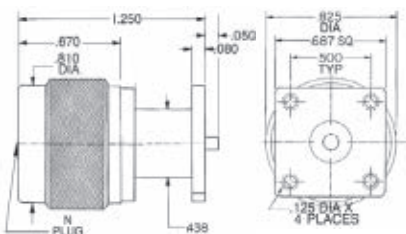
PART NO.	C DIM	D DIM	1-9	10-24	25-49	50-99	100+
1540-550 687 O	.160	.550	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75
1540-687 O	.050	.375	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75
1540-260 687 O	.200	.260	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75
1540-380 687 O	.050	.380	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75
1540-320 687 O	.055	.320	\$16.75	\$16.10	\$15.50	\$14.50	\$13.75



EXTENDED TERMINAL TNC FLANGE JACK CAPTIVE CONTACT

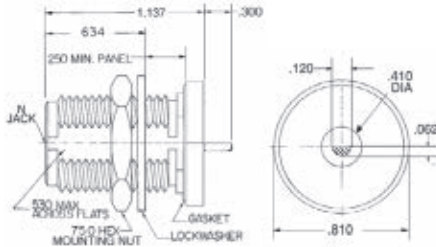
PART NO.	C DIM	D DIM	1-9	10-24	25-49	50-99	100+
1540-550-687	.160	.550	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25
1540-687	.050	.375	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25
1540-260-687	.200	.260	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25
1540-380-687	.050	.380	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25
1540-320-687	.055	.320	\$11.75	\$11.10	\$10.50	\$9.85	\$9.25

"N" Male Panel Mount & Female Bulkhead Feed Through Connectors



EXTENDED TERMINAL TNC FLANGE MOUNT PLUG CAPTIVE CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
1545-687	\$21.50	\$19.50	\$17.75	\$16.75	\$15.75



N JACK BULKHEAD FEED THROUGH EXTENDED TERMINAL D STYLE CAPTIVE CONTACT

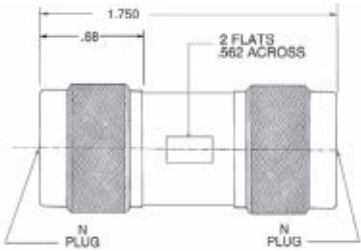
PART NO.	1-9	10-24	25-49	50-99	100+
1561	\$14.50	\$13.75	\$12.75	\$12.25	\$10.75

United Microwave Products Inc.

Direct Sales, Tech Support and Current Order Status

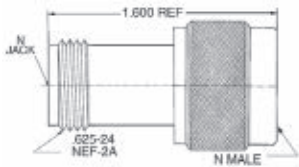
40 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 40

"N" In Series Adapters



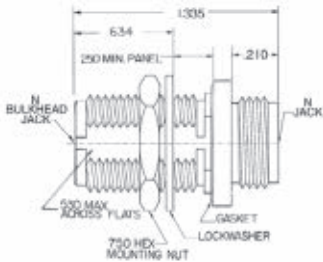
N PLUG TO N PLUG IN SERIES ADAPTER

PART NO.	1-9	10-24	25-49	50-99	100+
1551	\$59.50	\$56.25	\$52.50	\$47.50	\$42.50



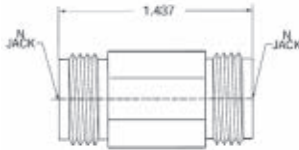
STRAIGHT ADAPTER PLUG N JACK TO N PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
1579	\$59.50	\$56.25	\$52.50	\$47.75	\$42.50



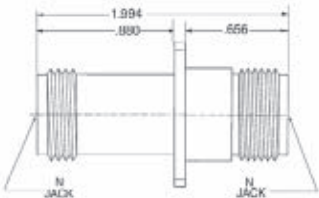
BULKHEAD FEED THROUGH MOUNT ADAPTER N JACK TO N JACK

PART NO.	1-9	10-24	25-49	50-99	100+
1550-BLK	\$99.50	\$96.75	\$92.75	\$87.50	\$84.50



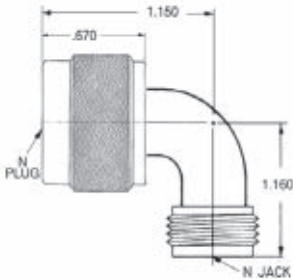
N JACK TO N JACK IN SERIES ADAPTER

PART NO.	1-9	10-24	25-49	50-99	100+
1550	\$59.50	\$56.25	\$52.50	\$47.75	\$42.50



N JACK TO N JACK ONE INCH FLANGE .125 DIA HOLES
4 PLACES FLANGE MOUNT IN SERIES ADAPTER

PART NO.	1-9	10-24	25-49	50-99	100+
1505	\$76.00	\$73.50	\$66.25	\$61.50	\$55.00



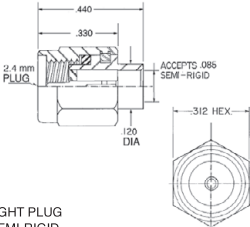
N JACK TO N PLUG RADIUS RIGHT ANGLE IN SERIES ADAPTER

PART NO.	1-9	10-24	25-49	50-99	100+
1521	\$142.00	\$135.00	\$127.00	\$119.00	\$112.00

High Performance Connectors

United Microwave Products High Performance SMP and Precision Semi-Rigid Connectors are constructed of metallic parts with a Gold Plated finish. All connectors listed on this page have Gold Plated BeCu center conductors and PTFE Dielectric as Per MIL-P-19468. The SMP connectors have been Qualified to US Navy DWG. 6783472 with A, B, & C testing including RF Leakage and Corona at Altitude.

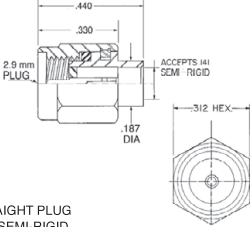
2.4mm Connectors



STRAIGHT PLUG
.085 SEMI-RIGID
WITH CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
301-1-2.4	\$22.75	\$21.50	\$18.50	\$17.25	\$16.95

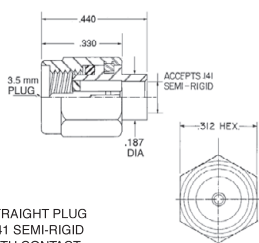
2.9mm Connectors



STRAIGHT PLUG
.141 SEMI-RIGID
WITH CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
300-7-2.9	\$18.50	\$17.25	\$16.75	\$15.50	\$14.25

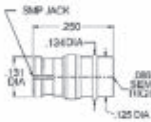
3.5mm Connectors



STRAIGHT PLUG
.141 SEMI-RIGID
WITH CONTACT

PART NO.	1-9	10-24	25-49	50-99	100+
300-7-3.5	\$49.50	\$47.75	\$42.50	\$39.00	\$37.50

SMP Type Connectors



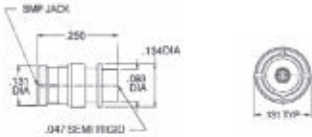
SMP .086 SEMI-RIGID CABLE STRAIGHT

PART NO.	1-9	10-24	25-49	50-99	100+
202-085	\$13.75	\$12.50	\$11.25	\$10.75	\$9.50



SMP JACK BULLET

PART NO.	1-9	10-24	25-49	50-99	100+
202-BT	\$16.50	\$15.50	\$14.75	\$13.75	\$12.50



SMP .047 SEMI-RIGID CABLE STRAIGHT ATTACHMENT

PART NO.	1-9	10-24	25-49	50-99	100+
202-047	\$13.75	\$12.50	\$11.25	\$10.75	\$9.50

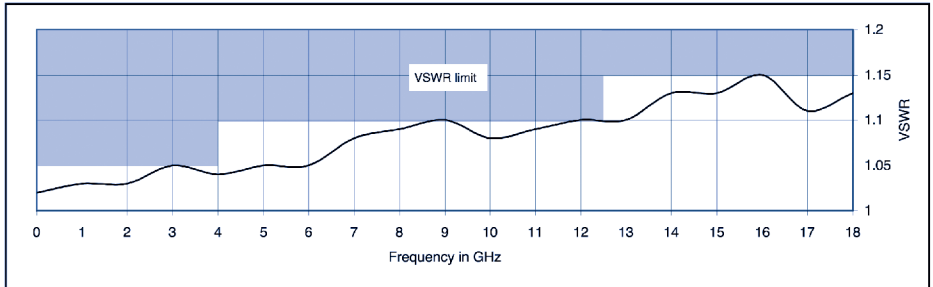


SMP FEMALE .086 SEMI-RIGID RIGHT ANGLE ATTACHMENT

PART NO.	1-9	10-24	25-49	50-99	100+
201-086	\$18.75	\$17.50	\$16.75	\$15.75	\$14.50

Between Series Coaxial Adapters

United Microwave Products between series coaxial adapters provide a convenient method for inner-connecting two different series or size coaxial connectors. Ideal for both measurement and systems use, these precision adapters offer a low VSWR over a broad frequency spectrum. In particular, the 7MM between series adapters are precision laboratory instruments used for testing microwave coaxial transmission lines. All standard units are constructed of stainless steel with a passivated finish, Teflon dielectrics, and gold plated beryllium copper center contacts. Panel mount adapters are available that permit small sized connectors for internal use while external connectors can be made with larger more rugged connectors

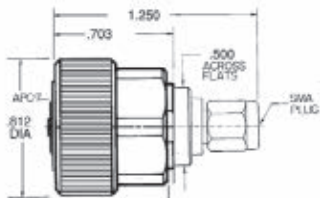


DATA FROM UMP PART # 1370



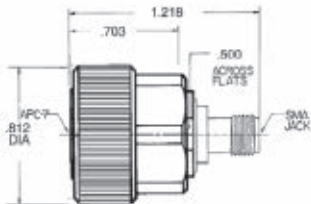
United Microwave Products Inc.
Direct Sales, Tech Support and Current Order Status

Between Series Coaxial Adapters



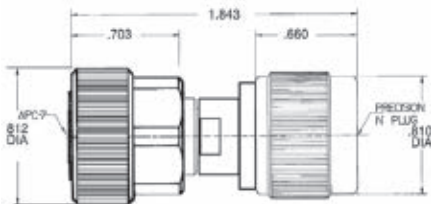
7mm TO SMA PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
9001	\$135.00	\$130.00	\$125.00	\$120.00	\$115.00



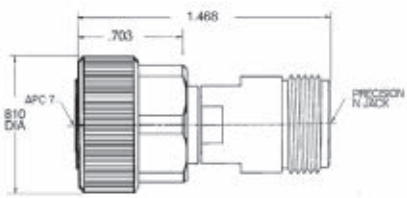
7mm TO SMA JACK

PART NO.	1-9	10-24	25-49	50-99	100+
9002	\$135.00	\$130.00	\$125.00	\$120.00	\$115.00



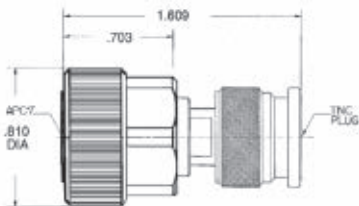
7mm TO N PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
9004	\$150.00	\$140.00	\$135.00	\$125.00	\$110.00



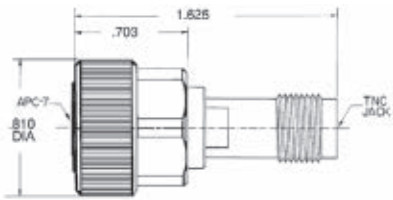
7mm TO N JACK

PART NO.	1-9	10-24	25-49	50-99	100+
9003	\$150.00	\$140.00	\$135.00	\$125.00	\$110.00



7mm TO TNC PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
9006	\$150.00	\$140.00	\$135.00	\$125.00	\$110.00



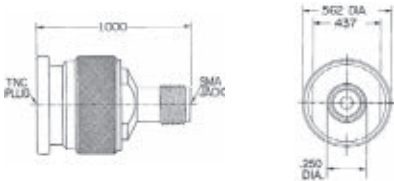
7mm TO TNC JACK

PART NO.	1-9	10-24	25-49	50-99	100+
9005	\$150.00	\$140.00	\$135.00	\$125.00	\$110.00

United Microwave Products Inc.

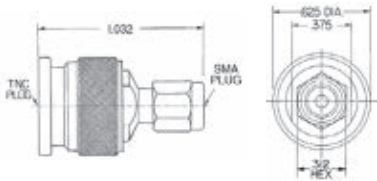
Direct Sales, Tech Support and Current Order Status

Between Series Coaxial Adapters



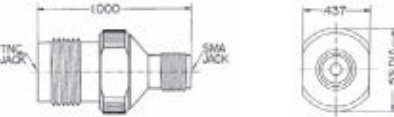
TNC PLUG TO SMA JACK

PART NO.	1-9	10-24	25-49	50-99	100+
7005	\$24.65	\$22.50	\$20.25	\$19.50	\$18.75



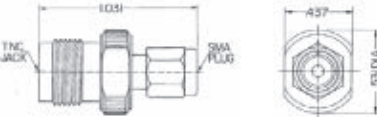
TNC PLUG TO SMA PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
7006	\$24.65	\$22.50	\$20.25	\$19.50	\$18.75



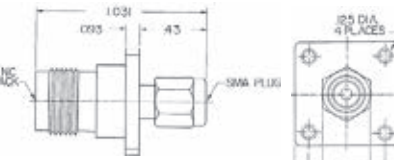
TNC JACK TO SMA JACK

PART NO.	1-9	10-24	25-49	50-99	100+
7002	\$24.65	\$22.50	\$20.25	\$19.50	\$18.75



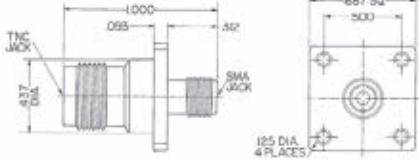
TNC JACK TO SMA PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
7003	\$24.65	\$22.50	\$20.25	\$19.50	\$18.75



TNC JACK TO SMA PLUG PANEL MOUNT FLANGE
MOUNT ALSO AVAILABLE WITH #3-56 THREADS
CONTACT FACTORY FOR DETAILS

PART NO.	1-9	10-24	25-49	50-99	100+
7004	\$32.00	\$29.50	\$27.75	\$26.75	\$24.75

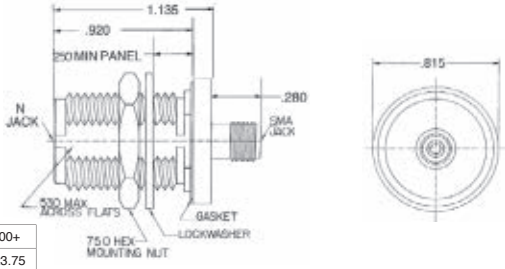


TNC JACK TO SMA JACK PANEL MOUNT FLANGE
MOUNT ALSO AVAILABLE WITH #3-56 THREADS
CONTACT FACTORY FOR DETAILS

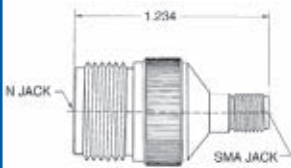
PART NO.	1-9	10-24	25-49	50-99	100+
7001	\$32.00	\$29.50	\$27.75	\$26.75	\$24.75

N JACK FEED THROUGH BULKHEAD TO
SMA JACK PANEL MOUNT

PART NO.	1-9	10-24	25-49	50-99	100+
1559BLK	\$29.50	\$27.75	\$26.75	\$24.75	\$23.75

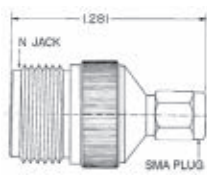


Between Series Coaxial Adapters



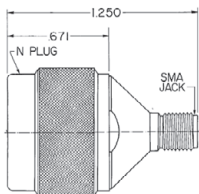
N JACK to SMA JACK

PART NO.	1-9	10-24	25-49	50-99	100+
1350	\$29.75	\$28.20	\$26.75	\$25.80	\$24.50



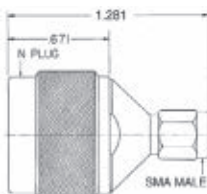
N JACK to SMA PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
1390	\$29.75	\$28.20	\$26.75	\$25.80	\$24.50



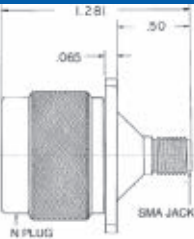
N PLUG to SMA JACK

PART NO.	1-9	10-24	25-49	50-99	100+
1370	\$29.75	\$28.20	\$26.75	\$25.80	\$24.50



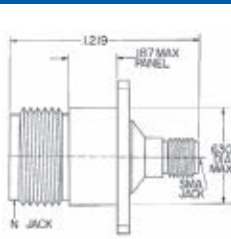
N PLUG to SMA PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
1400	\$29.75	\$28.20	\$26.75	\$25.80	\$24.50



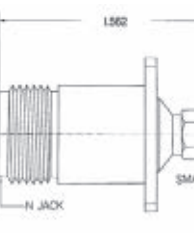
N PLUG to SMA JACK PANEL MOUNT

PART NO.	1-9	10-24	25-49	50-99	100+
1375	\$36.75	\$34.75	\$33.25	\$31.50	\$29.50



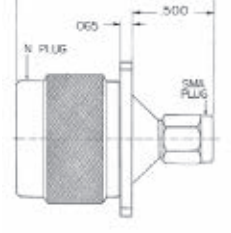
N JACK to SMA JACK PANEL MOUNT

PART NO.	1-9	10-24	25-49	50-99	100+
1355	\$36.75	\$34.75	\$33.25	\$31.50	\$29.50



N JACK to SMA PLUG PANEL MOUNT

PART NO.	1-9	10-24	25-49	50-99	100+
1395	\$36.75	\$34.75	\$33.25	\$31.50	\$29.50



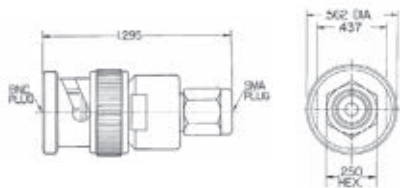
N PLUG to SMA PLUG PANEL MOUNT

PART NO.	1-9	10-24	25-49	50-99	100+
1405	\$36.75	\$34.75	\$33.25	\$31.50	\$29.50

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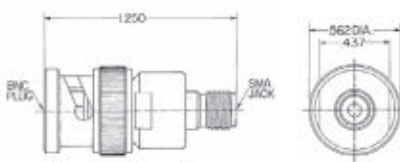
Direct Sales, Tech Support and Current Order Status

Between Series Coaxial Adapters



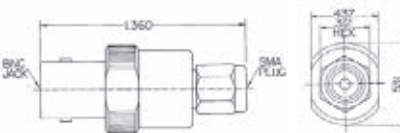
BNC PLUG TO SMA PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
1520	\$22.50	\$21.25	\$19.75	\$18.50	\$17.75



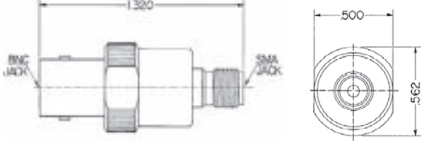
BNC PLUG TO SMA JACK

PART NO.	1-9	10-24	25-49	50-99	100+
1470	\$22.50	\$21.25	\$19.75	\$18.50	\$17.75



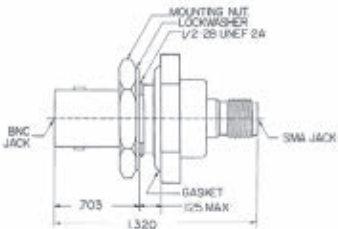
BNC JACK TO SMA PLUG

PART NO.	1-9	10-24	25-49	50-99	100+
1480	\$22.50	\$21.25	\$19.75	\$18.50	\$17.75



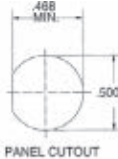
BNC JACK TO SMA JACK

PART NO.	1-9	10-24	25-49	50-99	100+
1450	\$22.50	\$21.25	\$19.75	\$18.50	\$17.75



BNC JACK TO SMA JACK
BULKHEAD MOUNT WITH GASKET

PART NO.	1-9	10-24	25-49	50-99	100+
7104	\$29.75	\$28.20	\$26.75	\$25.80	\$24.50



Custom Cable Assemblies

United Microwave Products offers a complete custom cable assembly facility to service your needs. High reliable cable assemblies, rigidly controlled to customer specifications are assembled by experienced personnel trained in the latest microwave assembly techniques. Precision bending and trimming, custom tool design, and total quality control assures that each assembly delivered to our customer meets our 100% Guaranteed performance, availability, plus reasonable cost makes United Microwave Products your number one choice for all cable assembly requirements. Contact us for complete technical and price information regarding your specific requirements.



AA-095-01.00.0



AA-098-01.00.0



CA-141-00.06.0 (3 CUSTOM BENDS SEMI-RIGID)



AA-155-01.00.0

UNITED MICROWAVE semi-rigid cable assemblies can also be custom formed and soldered to your intricate specifications (multiple bends, off tangent angles, three view drawings). All assemblies are fully tested and inspected per your requirements. Full tractability, material certs and source inspection are available upon request

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Custom Cable Assemblies

The Connector Selection Chart lists our most popular cables readily available. By following the directions under the assembly number explanation, it is possible to assign part numbers for an infinite variety of assemblies.

For instance, a 2' long 085 Tin plate semi-rigid cable with a SMA straight plug on one end and a SMA straight plug on the other would be part number AA-085Sn-02.00.0. Another example is a 10' long RG 142 cable with an SMA straight plug on one end and an SMA 90° plug on the other would be part number AB-142-10.00.0

CONNECTOR SELECTION CHART

- A - SMA Straight Plug
- B - SMA 90° Plug
- C - SMA Bulkhead Jack
- D - SMA Straight Jack
- E - SMA 2 Hole Captive Contact Jack
- G - TNC Straight Plug
- H - TNC Bulkhead Jack
- I - TNC 90° Plug
- J - BNC Straight Jack
- K - BNC Straight Plug
- L - BNC 90° Plug
- M - BNC Bulkhead Jack
- N - BNC Straight Plug
- O - N Straight Plug
- P - N 90° Plug
- R - N Straight Jack
- S - N Bulkhead Jack
- V - 7MM Straight Connector

SEMI-RIGID JACKET SELECTION

Ag - Silver

Cu - Bare Copper

Sn - Tin

CONNECTORS AVAILABLE IN
PASSIVATED STAINLESS STEEL FOR DURABILITY
OR BRASS SHELL FOR ECONOMY
GOLD, SILVER, NICKEL, FINISH
UPON REQUEST

Types of semi-rigid cable readily available:

.047, .085, .141, and .250

Outer jacket available in bare copper(Cu),
tin plated(Sn), silver plated(Ag), and spline.

Air filled and Helix cable are available on special
order.

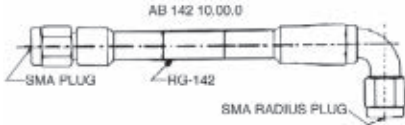
Types of RG cable readily available:

RG 55, 58, 142, 174, 178, 188,
223, 303, 315, 400

Types of Microflex cable readily available:

MICROFLEX 150, (FOIL OUTER CONDUCTOR)
MICROFLEX 155 & 095 (FOIL + BRAID OUTER CONDUCTOR)
MICROPOR 190 (AIR INDUCED DIELECTRIC)
MICROFLEX 165. (3 FOIL OUTER CONDUCTOR)

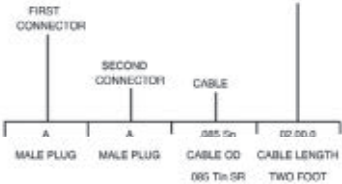
NOTE V.S.W.R. AND INSERTION LOSS LIMITS AS PER
CHOSEN CONNECTORS. CONTACT UNITED MICROWAVE
FOR CUSTOMER SERVICE & TECHNICAL SUPPORT



ASSEMBLY LENGTH

FIRST two digits represent feet while the next two digits
inches, and the last digit a tenth of an inch. Lengths are
measured to the reference plane of straight connectors
and to the center line of right angle connectors shown in
the assembly drawing

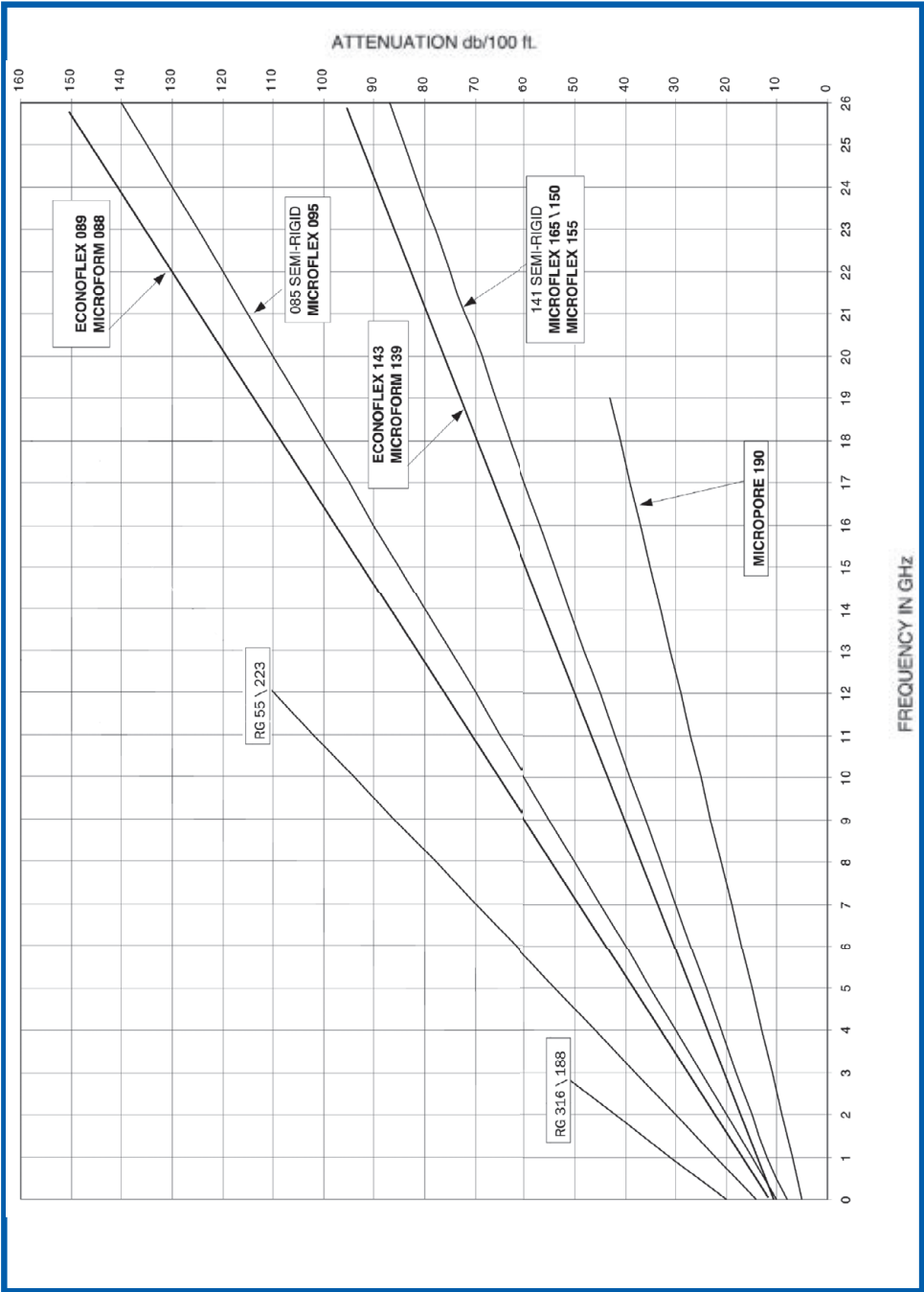
LENGTH	TOLERANCE
3" to 3'	- .25 INCH +0.5 INCH
3' to 6'	- .25 INCH +0.75 INCH
6' to 10'	- 1.50 INCH +2.50 INCH
10' to 20'	- 2.00 INCH +3.00 INCH



United Microwave Products Inc.

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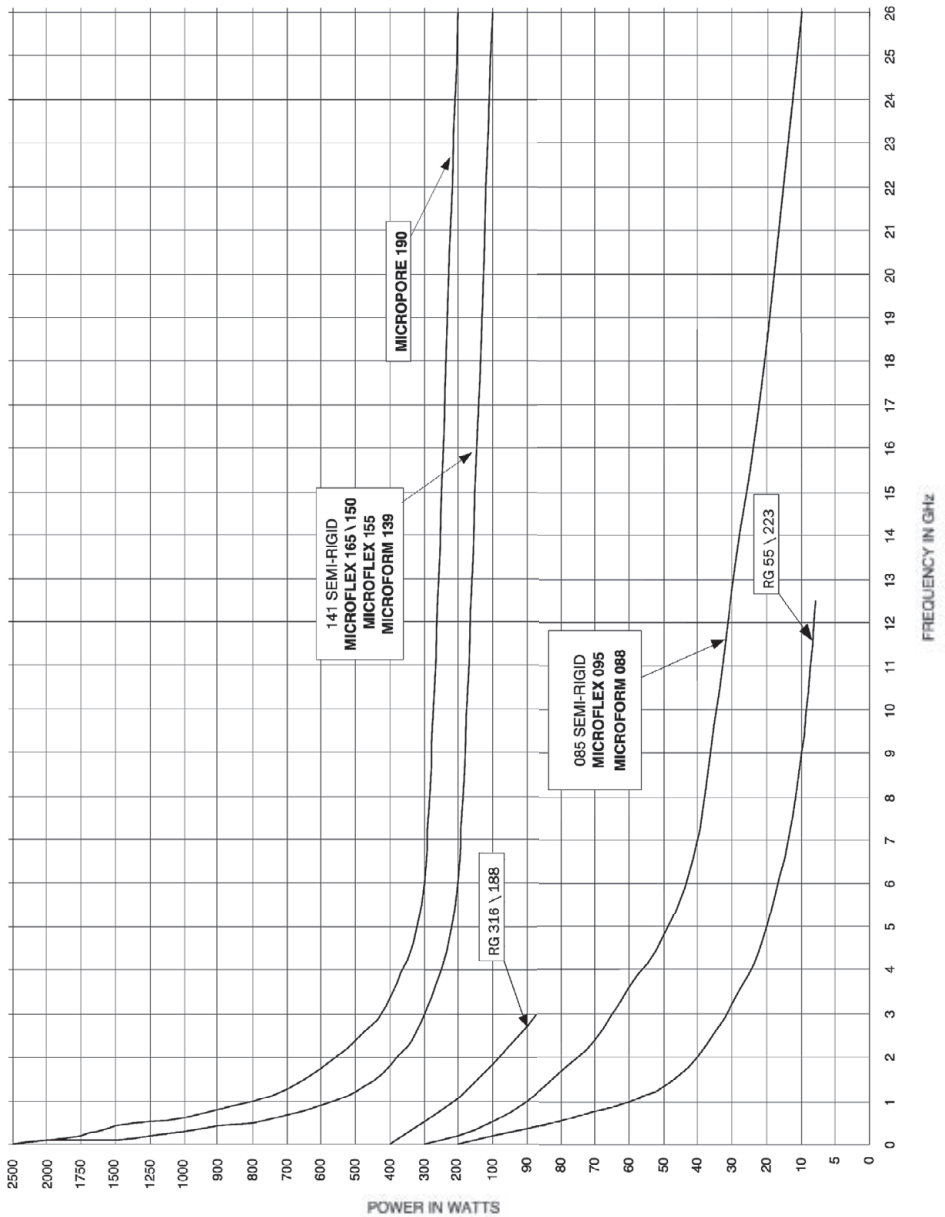


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MAXIMUM POWER HANDLING CAPABILITY OF POPULAR CABLES



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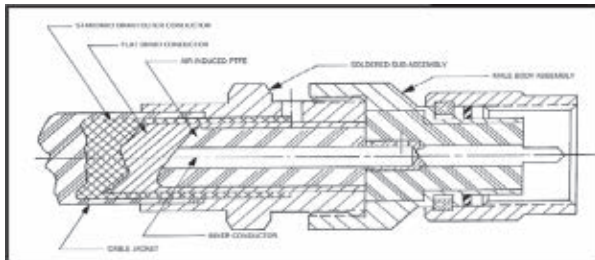
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Prices listed effective as of 1 July 2008 and subject to change at any time.

AFFORDABLE LOW LOSS TEST CABLES MICROPORE 190

Operating Frequency DC-18.0 GHz

MICROPORE 190 is a new inexpensive high performance super low loss cable. For applications requiring flexibility and the lowest possible loss at an economical price MICROPORE 190 is the cable of choice. The cable is nonmagnetic, has a double barrier outer conductor for improved shielding and features an air induced electric for low loss at high frequency.



ELECTRICAL PROPERTIES

Impedance 50 ± 2 OHMS
Cut off Frequency 33.0 GHz
Nominal Capacitance 25 pF
velocity of propagation 82.5%
Max Operating Voltage 1700 Volts RMS
RF Shielding Greater than 90db

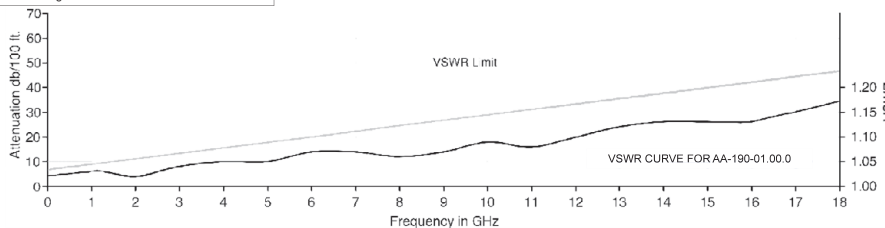
MATERIALS

Inner Conductor SIL PLT Solid Cu .051 Dia.
Outer Conductor Stripbraided Composite .184 Dia.
Dielectric Air Expanded PTFE .152 Dia.
Jacket FEP Teflon .195 Dia.

MECHANICAL PROPERTIES

Bend Radius Minimum 1.0 Inch
Temp Range -55°F/+400°F
Weight .6 oz/ft

— VSWR — Attenuation



SMA MALE TO SMA MALE

PART NO.	CONNECTORS	LENGTH	1-9	10-24	25-49
AA-190-02.00.0	SMA PLUG to SMA PLUG	2.00 Ft.	\$78.50	\$75.25	\$72.15
AA-190-03.00.0		3.00 Ft.	\$83.25	\$79.75	\$77.25
AA-190-04.00.0		4.00 Ft.	\$88.50	\$85.25	\$82.50
AA-190-05.00.0		5.00 Ft.	\$93.75	\$89.75	\$87.75
AA-190-06.00.0		6.00 Ft.	\$98.50	\$95.25	\$93.25
AA-190-10.00.0		10.00 Ft.	\$122.50	\$119.25	\$116.50

SMA MALE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH	1-9	10-24	25-49
AB-190-02.00.0	SMA PLUG to SMA PLUG RIGHT ANGLE	2.00 Ft.	\$109.50	\$107.25	\$104.75
AB-190-03.00.0		3.00 Ft.	\$115.50	\$113.25	\$110.75
AB-190-04.00.0		4.00 Ft.	\$121.50	\$119.25	\$116.75
AB-190-05.00.0		5.00 Ft.	\$127.50	\$125.75	\$122.75
AB-190-06.00.0		6.00 Ft.	\$133.50	\$131.25	\$128.75
AB-190-010.00.0		10.00 Ft.	\$157.50	\$155.25	\$153.75

SMA MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AO-190-02.00.0	SMA PLUG to TYPE "N" PLUG	2.00	\$101.50	\$98.25	\$95.75
AO-190-03.00.0		3.00	\$107.50	\$105.25	\$102.75
AO-190-04.00.0		4.00	\$113.50	\$110.25	\$107.75
AO-190-05.00.0		5.00	\$119.50	\$116.25	\$113.75
AO-190-06.00.0		6.00	\$125.50	\$122.25	\$119.75
AO-190-10.00.0		10.00	\$149.50	\$146.25	\$143.75

TYPE N MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
OO-190-02.00.0	TYPE "N" PLUG to TYPE "N" PLUG	2.00	\$120.50	\$118.00	\$115.25
OO-190-03.00.0		3.00	\$126.50	\$124.00	\$121.25
OO-190-04.00.0		4.00	\$132.50	\$130.00	\$127.25
OO-190-05.00.0		5.00	\$138.50	\$136.00	\$133.25
OO-190-06.00.0		6.00	\$144.50	\$142.00	\$139.25
OO-190-10.00.0		10.00	\$168.50	\$166.00	\$163.25

TYPE N MALE TO TYPE N MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH	1-9	10-24	25-49
OP-190-02.00.0	TYPE "N" PLUG to TYPE "N" PLUG RIGHT ANGLE	2.00 Ft.	\$150.50	\$148.00	\$145.25
OP-190-03.00.0		3.00 Ft.	\$156.50	\$154.00	\$151.25
OP-190-04.00.0		4.00 Ft.	\$162.50	\$160.00	\$157.25
OP-190-05.00.0		5.00 Ft.	\$168.50	\$166.00	\$163.25
OP-190-06.00.0		6.00 Ft.	\$174.50	\$172.00	\$169.25
OP-190-10.00.0		10.00 Ft.	\$198.50	\$196.00	\$193.25

For Connectors or Lengths not listed contact Factory.

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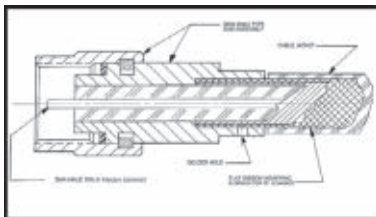
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Prices listed effective as of 1 July 2008 and subject to change at any time.

AFFORDABLE TEST CABLES MICROFLEX 155

Operating Frequency DC-18.0 GHz

MICROFLEX 155 is a new inexpensive standard duty test cable. For applications requiring flexibility at an economical price MICROFLEX 155 is the cable of choice. The cable is has a double barrier outer conductor for improved shielding at high frequency.



ELECTRICAL PROPERTIES

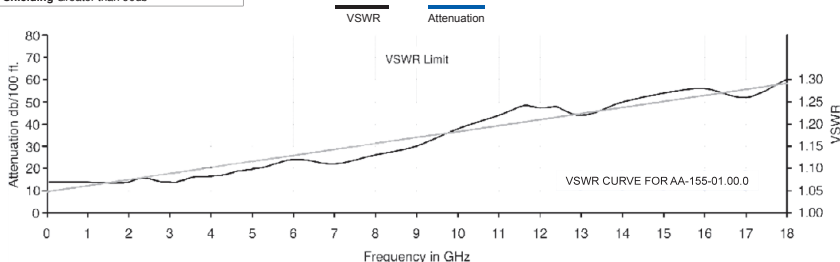
Impedance 50 ± 2 OHms
Cut off Frequency 33.0 GHz
Nominal Capacitance 29.4 pF/ft
Velocity of propagation 69.5%
Max Operating Voltage 1200 Volts RMS
RF Shielding Greater than 90db

MATERIALS

Inner Conductor SIL PLT Cu Clad Steel .036 Dia.
Outer Conductor Cu Ribbon & Braid .135 Dia.
Dielectric Solid PTFE .116 Dia.
Jacket FEP Teflon .155 Dia.

MECHANICAL PROPERTIES

Bend Radius Minimum 1.0 Inch
Temp Range -55°F/+400°F
Weight .47 oz/ft



SMA MALE TO SMA MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AA-155-02.00.0	SMA PLUG to SMA PLUG	2.0	\$66.50	\$65.25	\$64.15
AA-155-03.00.0		3.0	\$69.25	\$68.75	\$67.25
AA-155-04.00.0		4.0	\$72.50	\$71.25	\$70.50
AA-155-05.00.0		5.0	\$75.75	\$74.75	\$73.75
AA-155-06.00.0		6.0	\$78.50	\$77.25	\$76.25
AA-155-10.00.0		10.0	\$89.50	\$88.25	\$87.50

TYPE N MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
OO-155-02.00.0	TYPE "N" PLUG to TYPE "N" PLUG	2.0	\$93.50	\$92.50	\$91.50
OO-155-03.00.0		3.0	\$96.50	\$95.50	\$94.50
OO-155-04.00.0		4.0	\$99.50	\$98.50	\$97.50
OO-155-05.00.0		5.0	\$102.50	\$101.50	\$100.50
OO-155-06.00.0		6.0	\$105.50	\$104.50	\$103.50
OO-155-10.00.0		10.0	\$117.50	\$116.50	\$115.50

SMA MALE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AB-155-02.00.0	SMA PLUG to SMA PLUG RIGHT ANGLE	2.0 Ft.	\$91.50	\$90.50	\$89.50
AB-155-03.00.0		3.0 Ft.	\$94.50	\$93.50	\$92.50
AB-155-04.00.0		4.0 Ft.	\$97.50	\$96.50	\$95.50
AB-155-05.00.0		5.0 Ft.	\$100.50	\$99.50	\$98.50
AB-155-06.00.0		6.0 Ft.	\$103.50	\$102.50	\$101.50
AB-155-10.00.0		10.0 Ft.	\$115.50	\$114.50	\$113.50

TYPE N MALE TO TYPE N MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
OP-155-02.00.0	TYPE "N" PLUG to TYPE "N" RIGHT ANGLE PLUG	2.0	\$114.50	\$113.50	\$112.50
OP-155-03.00.0		3.0	\$117.50	\$116.50	\$115.50
OP-155-04.00.0		4.0	\$120.50	\$119.50	\$118.50
OP-155-05.00.0		5.0	\$123.50	\$122.50	\$121.50
OP-155-06.00.0		6.0	\$126.50	\$125.50	\$124.50
OP-155-10.00.0		10.0	\$138.50	\$137.50	\$136.50

SMA MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AO-155-02.00.0	SMA PLUG to TYPE "N" PLUG	2.0	\$82.50	\$81.50	\$80.50
AO-155-03.00.0		3.0	\$85.50	\$84.50	\$83.50
AO-155-04.00.0		4.0	\$88.50	\$87.50	\$86.50
AO-155-05.00.0		5.0	\$91.50	\$90.50	\$89.50
AO-155-06.00.0		6.0	\$94.50	\$93.50	\$92.50
AO-155-10.00.0		10.0	\$106.50	\$105.50	\$104.50

For Connectors or Lengths not listed contact Factory.

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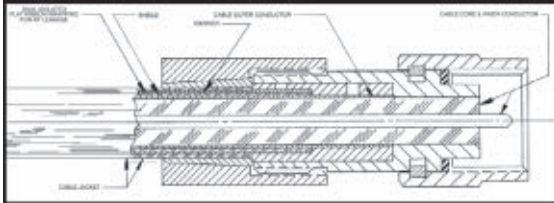
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MICROFLEX 165

Operating Frequency DC-26.0 GHz

MICROFLEX 165 is designed for high isolation and stability under demanding conditions. It features a totally **NONMAGNETIC** construction with a fused laminated PTFE core. The shielding characteristics are unsurpassed in a flexible cable. MICROFLEX 165 has a finished diameter of .165 inch. The SMA connectors are passivated stainless steel and feature a thick wall design for durability and repeated mating cycles. The inner conductor and core become an integral part of the SMA connector for better VSWR and electrical characteristics. MICROFLEX 165 cable assemblies are designed to provide maximum durability, shielding and electrical performance under extremes of handling, vibration and environmental exposure



ELECTRICAL PROPERTIES

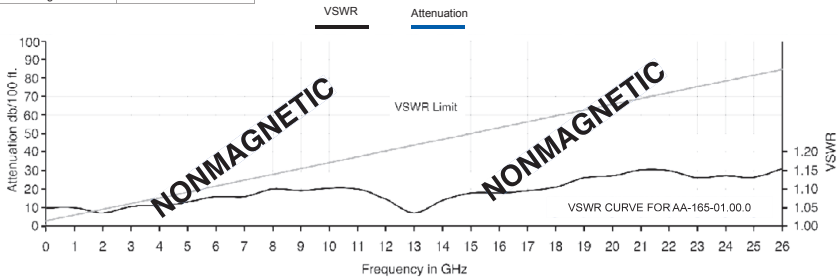
Impedance	50 ± 1 OHM
velocity of propagation	69.5%
Cut off Frequency	35.0 GHz
Max Operating Voltage	1900 Volts RMS
Nominal Capacitance	29.4 pF/ft
RF Shielding	Greater than 90db

MATERIALS

Inner Conductor	SIL PLT. Be Cu .036 Dia.
Dielectric	PTFE .116 Dia.
Outer Conductor	Dual Isolated SIL PLT Copper Ribbon .140 Dia.
Jacket	FEP Teflon .165 Dia.

MECHANICAL PROPERTIES

Bend Radius	Minimum 1.0 Inch
Weight	.6 oz/ft
Temp Range	-55°F/+400°F



SMA MALE TO SMA MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AA-165-00.06.0	SMA PLUG to SMA PLUG	0.6	\$74.50	\$72.00	\$69.50
AA-165-01.00.0		1.0	\$74.50	\$72.00	\$69.50
AA-165-01.06.0		1.5	\$77.50	\$75.00	\$72.50
AA-165-02.00.0		2.0	\$80.50	\$78.00	\$75.50
AA-165-02.06.0		2.5	\$83.50	\$81.00	\$78.50
AA-165-03.00.0		3.0	\$86.50	\$84.00	\$81.50
AA-165-04.00.0		4.0	\$92.50	\$90.00	\$87.50
AA-165-05.00.0		5.0	\$98.50	\$96.00	\$93.50
AA-165-06.00.0		6.0	\$104.50	\$102.00	\$99.50
AA-165-10.00.0		10.0	\$128.50	\$126.00	\$105.50

SMA MALE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH	1-9	10-24	25-49
AB-165-00.06.0	SMA PLUG to SMA PLUG RIGHT ANGLE	0.5 Ft.	\$114.50	\$112.00	\$109.50
AB-165-01.00.0		1.0 Ft.	\$114.50	\$112.00	\$109.50
AB-165-01.06.0		1.5 Ft.	\$117.50	\$115.00	\$112.50
AB-165-02.00.0		2.0 Ft.	\$120.50	\$118.00	\$115.50
AB-165-02.06.0		2.5 Ft.	\$123.50	\$121.00	\$118.50
AB-165-03.00.0		3.0 Ft.	\$126.50	\$124.00	\$121.50
AB-165-04.00.0		4.0 Ft.	\$132.50	\$130.00	\$127.50
AB-165-05.00.0		5.0 Ft.	\$138.50	\$136.00	\$133.50
AB-165-06.00.0		6.0 Ft.	\$144.50	\$142.00	\$139.50
AB-165-10.00.0		10.0 Ft.	\$168.50	\$166.00	\$163.50

SMA MALE TO SMA BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AC-165-01.00.0	SMA PLUG to SMA BULKHEAD JACK	1.0	\$94.50	\$92.50	\$89.50
AC-165-01.06.0		1.5	\$97.50	\$95.00	\$92.50
AC-165-02.00.0		2.0	\$100.50	\$98.00	\$95.50
AC-165-02.06.0		2.5	\$103.50	\$101.00	\$98.50
AC-165-03.00.0		3.0	\$106.50	\$104.00	\$101.50
AC-165-04.00.0		4.0	\$112.50	\$110.00	\$107.50
AC-165-05.00.0		5.0	\$118.50	\$116.00	\$113.50
AC-165-06.00.0		6.0	\$124.50	\$122.00	\$119.50

SMA MALE RIGHT ANGLE TO SMA MALE RIGHT ANGLE

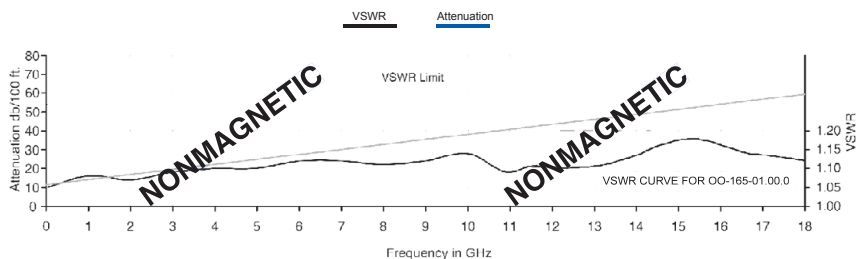
PART NO.	CONNECTORS	LENGTH	1-9	10-24	25-49
BB-165-00.06.0	SMA PLUG RIGHT ANGLE to SMA PLUG RIGHT ANGLE	0.5 Ft.	\$143.50	\$141.00	\$135.50
BB-165-01.00.0		1.0 Ft.	\$143.50	\$141.00	\$138.50
BB-165-01.06.0		1.5 Ft.	\$146.50	\$144.00	\$141.50
BB-165-02.00.0		2.0 Ft.	\$149.50	\$147.00	\$144.50
BB-165-02.06.0		2.5 Ft.	\$152.50	\$150.00	\$147.50
BB-165-03.00.0		3.0 Ft.	\$155.50	\$153.00	\$150.50
BB-165-04.00.0		4.0 Ft.	\$161.50	\$159.00	\$156.50
BB-165-05.00.0		5.0 Ft.	\$167.50	\$165.00	\$162.50
BB-165-06.00.0		6.0 Ft.	\$173.50	\$171.00	\$168.50

United Microwave Products Inc.

Direct Sales, Tech Support and Current Order Status

MICROFLEX 165

Operating Frequency DC-18.0 GHz



SMA MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AO-165-01.00.0	SMA PLUG to TYPE "N" PLUG	1.0	\$95.50	\$93.00	\$90.50
AO-165-01.06.0		1.5	\$98.50	\$96.00	\$93.50
AO-165-02.00.0		2.0	\$101.50	\$99.00	\$96.50
AO-165-02.06.0		2.5	\$104.50	\$102.00	\$99.50
AO-165-03.00.0		3.0	\$107.50	\$105.00	\$102.50
AO-165-04.00.0		4.0	\$113.50	\$111.00	\$108.50
AO-165-05.00.0		5.0	\$119.50	\$117.00	\$114.50
AO-165-06.00.0		6.0	\$125.50	\$123.00	\$120.50

TYPE N MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
OO-165-01.00.0	TYPE "N" PLUG to TYPE "N" PLUG	1.0	\$105.50	\$103.00	\$100.50
OO-165-01.06.0		1.5	\$108.50	\$106.00	\$103.50
OO-165-02.00.0		2.0	\$111.50	\$109.00	\$106.50
OO-165-02.06.0		2.5	\$114.50	\$112.00	\$109.50
OO-165-03.00.0		3.0	\$117.50	\$115.00	\$112.50
OO-165-04.00.0		4.0	\$123.50	\$121.00	\$118.50
OO-165-05.00.0		5.0	\$129.50	\$127.00	\$124.50
OO-165-06.00.0		6.0	\$135.50	\$133.00	\$130.50

SMA MALE TO TYPE N BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AS-165-01.00.0	SMA PLUG to TYPE "N" BULKHEAD JACK	1.0	\$105.50	\$103.00	\$100.50
AS-165-01.06.0		1.5	\$108.50	\$106.00	\$103.50
AS-165-02.00.0		2.0	\$111.50	\$109.00	\$106.50
AS-165-02.06.0		2.5	\$114.50	\$112.00	\$109.50
AS-165-03.00.0		3.0	\$117.50	\$115.00	\$112.50
AS-165-04.00.0		4.0	\$123.50	\$121.00	\$118.50
AS-165-05.00.0		5.0	\$129.50	\$127.00	\$124.50
AS-165-06.00.0		6.0	\$135.50	\$133.00	\$130.50

TNC MALE TO TNC MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
GG-165-01.00.0	TNC PLUG to TNC PLUG	1.0	\$144.50	\$142.00	\$139.50
GG-165-01.06.0		1.5	\$146.50	\$144.00	\$141.50
GG-165-02.00.0		2.0	\$149.50	\$147.00	\$144.50
GG-165-02.06.0		2.5	\$152.50	\$150.00	\$147.50
GG-165-03.00.0		3.0	\$155.50	\$153.00	\$150.50
GG-165-04.00.0		4.0	\$161.50	\$159.00	\$156.50
GG-165-05.00.0		5.0	\$167.50	\$165.00	\$162.50
GG-165-06.00.0		6.0	\$173.50	\$171.00	\$168.50

SMA MALE TO TNC MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AG-165-01.00.0	SMA PLUG to TNC PLUG	1.0	\$117.50	\$115.00	\$112.50
AG-165-01.06.0		1.5	\$120.50	\$118.00	\$115.50
AG-165-02.00.0		2.0	\$123.50	\$121.00	\$118.50
AG-165-02.06.0		2.5	\$126.50	\$124.00	\$121.50
AG-165-03.00.0		3.0	\$132.50	\$130.00	\$127.50
AG-165-04.00.0		4.0	\$138.50	\$136.00	\$133.50
AG-165-05.00.0		5.0	\$144.50	\$142.00	\$139.50
AG-165-06.00.0		6.0	\$168.50	\$166.00	\$163.50

TYPE N MALE TO TYPE N BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
OS-165-01.00.0	TYPE "N" PLUG to TYPE "N" BULKHEAD JACK	1.0	\$115.50	\$113.00	\$110.50
OS-165-01.06.0		1.5	\$118.50	\$116.00	\$113.50
OS-165-02.00.0		2.0	\$121.50	\$119.00	\$116.50
OS-165-02.06.0		2.5	\$124.50	\$122.00	\$119.50
OS-165-03.00.0		3.0	\$127.50	\$125.00	\$122.50
OS-165-04.00.0		4.0	\$133.50	\$131.00	\$128.50
OS-165-05.00.0		5.0	\$139.50	\$137.00	\$134.50
OS-165-06.00.0		6.0	\$145.50	\$143.00	\$140.50

United Microwave Products Inc.

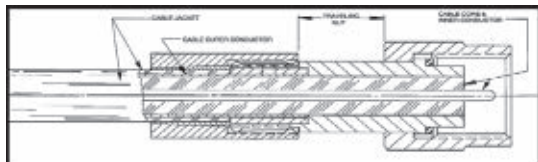
Direct Sales, Tech Support and Current Order Status

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MICROFLEX 150

Operating Frequency DC-26.0 GHz

MICROFLEX 150 is a flexible cable replacement for .141 semi-rigid delivering the same electrical performance. The standard stainless steel SMA connectors feature a thick wall construction for durability through repeated mating cycles. The coupling nut retracts for visual mating of the center conductors. The connector design is such that the core and center conductor become an integral part of the SMA connector. The use of MICROFLEX 150 eliminates complicated three plane drawing required with complex semi-rigid designs, often allowing one part number to replace several different cables. The flexibility of MICROFLEX 150 also eliminates cracked or broken solder joints caused by misalignment of semi-rigid cables during mating, while retaining the electrical performance of .141 semi-rigid.



ELECTRICAL PROPERTIES

Impedance	50 ± 1 OHM
velocity of propagation	69.5%
Cut off Frequency	35.0 GHz
Max Operating Voltage	1900 Volts RMS
Nominal Capacitance	29.4 pff
RF Shielding	Greater than 90db

MATERIALS

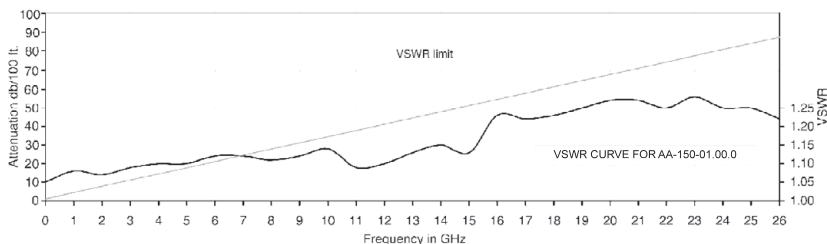
Inner Conductor	SIL PLT. Cu Clad Steel.036 Dia.
Dielectric	PTFE .116 Dia.
Outer Conductor	SIL PLT Copper Ribbon .125 Dia.
Jacket	FEP Teflon .150 Dia.

MECHANICAL PROPERTIES

Bend Radius	Minimum 1.0 Inch
Weight	4 oz/ft
Temp Range	-55°F/+400°F

VSWR

Attenuation



SMA MALE TO SMA MALE

PART NO.	CONNECTORS	LENGTH (FT.)	1-9	10-24	25-49
AA-150-00.06.0	SMA PLUG to SMA PLUG	0.6	\$37.50	\$36.50	\$35.50
AA-150-01.00.0		1.0	\$39.50	\$38.50	\$37.50
AA-150-01.06.0		1.5	\$41.50	\$40.50	\$39.50
AA-150-02.00.0		2.0	\$43.50	\$42.50	\$41.50
AA-150-02.06.0		2.5	\$45.50	\$44.50	\$43.50
AA-150-03.00.0		3.0	\$47.50	\$46.50	\$45.50
AA-150-04.00.0		4.0	\$51.50	\$50.50	\$49.50
AA-150-05.00.0		5.0	\$55.50	\$54.50	\$53.50
AA-150-06.00.0		6.0	\$59.50	\$58.50	\$57.50
AA-150-10.00.0		10.0	\$75.50	\$74.50	\$73.50

SMA MALE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH	1-9	10-24	25-49
AB-150-00.06.0	SMA PLUG to SMA PLUG RIGHT ANGLE	0.6 Ft.	\$80.25	\$79.25	\$78.25
AB-150-01.00.0		1.0 Ft.	\$82.25	\$81.25	\$80.25
AB-150-01.06.0		1.5 Ft.	\$84.25	\$83.25	\$82.25
AB-150-02.00.0		2.0 Ft.	\$86.25	\$85.25	\$84.25
AB-150-02.06.0		2.5 Ft.	\$88.25	\$87.25	\$86.25
AB-150-03.00.0		3.0 Ft.	\$90.25	\$89.25	\$88.25
AB-150-04.00.0		4.0 Ft.	\$94.25	\$93.25	\$92.25
AB-150-05.00.0		5.0 Ft.	\$98.25	\$97.25	\$96.25
AB-150-06.00.0		6.0 Ft.	\$102.25	\$101.25	\$100.25
AB-150-10.00.0		10.0 Ft.	\$118.25	\$117.25	\$116.25

SMA MALE TO SMA BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (FT.)	1-9	10-24	25-49
AC-150-01.00.0	SMA PLUG to SMA BULKHEAD JACK	1.0	\$54.00	\$53.00	\$52.00
AC-150-01.06.0		1.5	\$57.00	\$56.00	\$55.00
AC-150-02.00.0		2.0	\$60.00	\$59.00	\$58.00
AC-150-02.06.0		2.5	\$63.00	\$62.00	\$61.00
AC-150-03.00.0		3.0	\$64.50	\$63.50	\$62.50
AC-150-04.00.0		4.0	\$69.00	\$68.00	\$67.00
AC-150-05.00.0		5.0	\$74.25	\$73.25	\$72.25
AC-150-06.00.0		6.0	\$79.50	\$78.50	\$77.50

SMA MALE RIGHT ANGLE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH	1-9	10-24	25-49
BB-150-00.06.0	SMA PLUG RIGHT ANGLE to SMA PLUG RIGHT ANGLE	0.6 Ft.	\$126.00	\$125.00	\$124.00
BB-150-01.00.0		1.0 Ft.	\$126.00	\$125.00	\$124.00
BB-150-01.06.0		1.5 Ft.	\$129.00	\$128.00	\$127.00
BB-150-02.00.0		2.0 Ft.	\$132.00	\$131.00	\$130.00
BB-150-02.06.0		2.5 Ft.	\$135.00	\$134.00	\$133.00
BB-150-03.00.0		3.0 Ft.	\$138.00	\$137.00	\$136.00
BB-150-04.00.0		4.0 Ft.	\$144.00	\$143.00	\$142.00
BB-150-05.00.0		5.0 Ft.	\$150.00	\$149.00	\$148.00
BB-150-06.00.0		6.0 Ft.	\$156.00	\$155.00	\$154.00

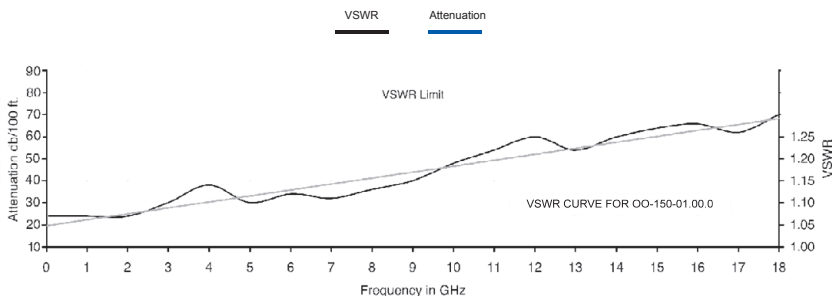
United Microwave Products Inc.

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MICROFLEX 150

Operating Frequency DC-18.0 GHz



SMA MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AO-150-01.00.0	SMA PLUG to TYPE "N" PLUG	1.0	\$57.75	\$56.75	\$55.75
AO-150-01.06.0		1.5	\$60.00	\$59.00	\$58.05
AO-150-02.00.0		2.0	\$62.25	\$61.25	\$60.25
AO-150-02.06.0		2.5	\$64.50	\$63.50	\$62.50
AO-150-03.00.0		3.0	\$66.75	\$65.75	\$64.75
AO-150-04.00.0		4.0	\$71.25	\$70.25	\$69.25
AO-150-05.00.0		5.0	\$75.75	\$74.75	\$73.75
AO-150-06.00.0		6.0	\$80.25	\$79.25	\$78.25
AO-150-10.00.0		10.0	\$98.25	\$97.25	\$96.25

TYPE N MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
OO-150-01.00.0	TYPE "N" PLUG to TYPE "N" PLUG	1.0	\$66.75	\$65.75	\$64.75
OO-150-01.06.0		1.5	\$69.00	\$68.00	\$67.00
OO-150-02.00.0		2.0	\$72.00	\$71.00	\$70.00
OO-150-02.06.0		2.5	\$74.25	\$73.25	\$72.25
OO-150-03.00.0		3.0	\$76.50	\$75.50	\$74.50
OO-150-04.00.0		4.0	\$81.75	\$80.75	\$79.75
OO-150-05.00.0		5.0	\$86.25	\$85.25	\$84.25
OO-150-06.00.0		6.0	\$91.50	\$90.50	\$89.50
OO-150-10.00.0		10.0	\$108.75	\$107.75	\$106.75

SMA MALE TO TYPE N BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AS-150-01.00.0	SMA PLUG to TYPE "N" BULKHEAD JACK	1.0	\$67.50	\$66.50	\$65.50
AS-150-01.06.0		1.5	\$69.75	\$68.75	\$67.75
AS-150-02.00.0		2.0	\$72.00	\$71.00	\$70.00
AS-150-02.06.0		2.5	\$74.25	\$73.25	\$72.25
AS-150-03.00.0		3.0	\$76.50	\$75.50	\$74.50
AS-150-04.00.0		4.0	\$81.00	\$80.00	\$79.00
AS-150-05.00.0		5.0	\$85.50	\$84.50	\$83.50
AS-150-06.00.0		6.0	\$90.00	\$89.00	\$88.00

TNC MALE TO TNC MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
GG-150-01.00.0	TNC PLUG to TNC PLUG	1.0	\$81.00	\$80.00	\$79.00
GG-150-01.06.0		1.5	\$84.00	\$83.00	\$82.00
GG-150-02.00.0		2.0	\$87.00	\$86.00	\$85.00
GG-150-02.06.0		2.5	\$89.25	\$88.25	\$87.25
GG-150-03.00.0		3.0	\$91.50	\$90.50	\$89.50
GG-150-04.00.0		4.0	\$96.00	\$95.00	\$94.00
GG-150-05.00.0		5.0	\$101.25	\$100.25	\$99.25
GG-150-06.00.0		6.0	\$106.50	\$105.50	\$104.50

SMA MALE TO TNC MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
AG-150-01.00.0	SMA PLUG to TNC PLUG	1.0	\$60.75	\$59.75	\$58.75
AG-150-01.06.0		1.5	\$63.75	\$62.75	\$61.75
AG-150-02.00.0		2.0	\$66.00	\$65.00	\$64.00
AG-150-02.06.0		2.5	\$68.25	\$67.25	\$66.25
AG-150-03.00.0		3.0	\$71.25	\$70.25	\$69.25
AG-150-04.00.0		4.0	\$75.75	\$74.75	\$73.75
AG-150-05.00.0		5.0	\$81.00	\$80.00	\$79.00
AG-150-06.00.0		6.0	\$85.50	\$84.50	\$83.50

TYPE N MALE TO TYPE N BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
OS-150-01.00.0	TYPE "N" PLUG to TYPE "N" BULKHEAD JACK	1.0	\$80.25	\$79.25	\$78.25
OS-150-01.06.0		1.5	\$82.50	\$81.50	\$80.50
OS-150-02.00.0		2.0	\$84.75	\$83.75	\$82.75
OS-150-02.06.0		2.5	\$87.00	\$86.00	\$85.00
OS-150-03.00.0		3.0	\$89.25	\$88.25	\$87.25
OS-150-04.00.0		4.0	\$93.75	\$92.75	\$91.75
OS-150-05.00.0		5.0	\$98.25	\$97.25	\$96.25
OS-150-06.00.0		6.0	\$102.75	\$101.75	\$100.75

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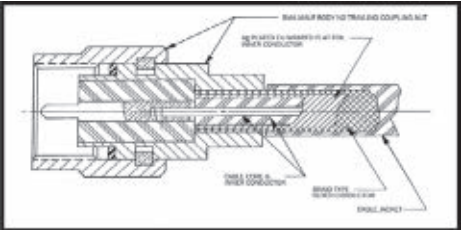
Direct Sales, Tech Support and Current Order Status

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MICROFLEX 095

Operating Frequency DC-18.0 GHz

MICROFLEX 095 is a miniature flexible cable with the approximate size and electrical characteristics of .085 semirigid at a price comparable to an RG-316 assembly and the flexibility of RG-188. The cable is approximately half the size of RG-142 with 4 to 5 times the flexibility. MICROFLEX 095 has a finished diameter of .095 inch. The cable is designed to offer excellent shielding characteristics and good flexibility while maintaining the attenuation performance of .085 semi-rigid.



ELECTRICAL PROPERTIES

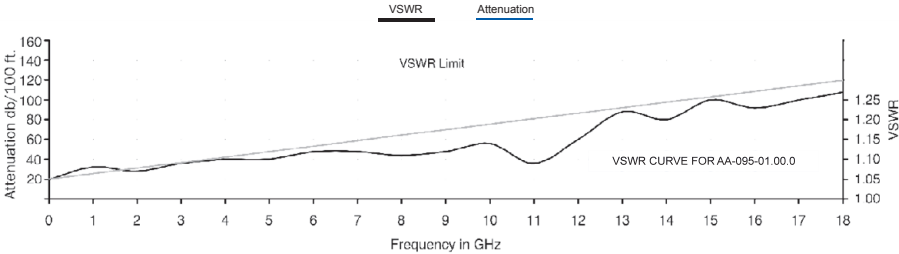
Impedance	50 ± 1 OHM
velocity of propagation	69.5%
Cut off Frequency	60.0 GHz
Max Operating Voltage	1200 Volts RMS
Nominal Capacitance	29.4 ptf/ft
RF Shielding	Greater than 90db

MATERIALS

Inner Conductor	SIL. PLT. Cu Clad Steel .020 Dia.
Dielectric	PTFE .066 Dia.
Outer Conductor	SIL. PLT Copper Ribbon .080 Dia.
Jacket	FEP Teflon .095 Dia.

MECHANICAL PROPERTIES

Bend Radius	Minimum 0.5 Inch
Weight	.175 oz/ft
Temp Range	-55°F/+400°F



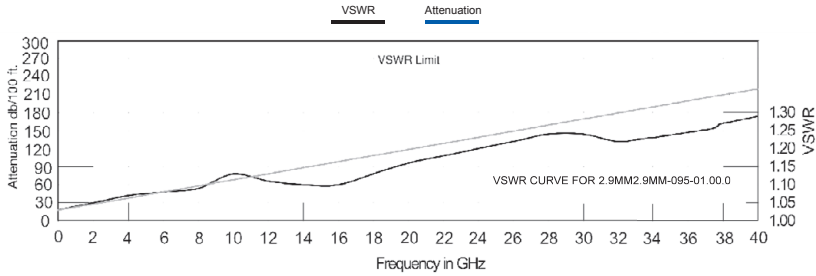
SMA MALE TO SMA MALE

PART NO.	CONNECTORS	LENGTH (FL)	1-9	10-24	25-49
AA-095-00.06.0	SMA PLUG to SMA PLUG	0.6	\$25.00	\$24.00	\$23.00
AA-095-01.00.0		1.0	\$25.00	\$24.00	\$23.00
AA-095-01.06.0		1.5	\$27.00	\$26.00	\$25.00
AA-095-02.00.0		2.0	\$29.00	\$28.00	\$27.00
AA-095-02.06.0		2.5	\$31.00	\$30.00	\$29.00
AA-095-03.00.0		3.0	\$33.00	\$32.00	\$31.00
AA-095-04.00.0		4.0	\$37.00	\$36.00	\$35.00
AA-095-05.00.0		5.0	\$41.00	\$40.00	\$39.00
AA-095-06.00.0		6.0	\$45.00	\$44.00	\$43.00

Prices listed effective as of 1 July 2008 and subject to change at any time.

MICROFLEX 095

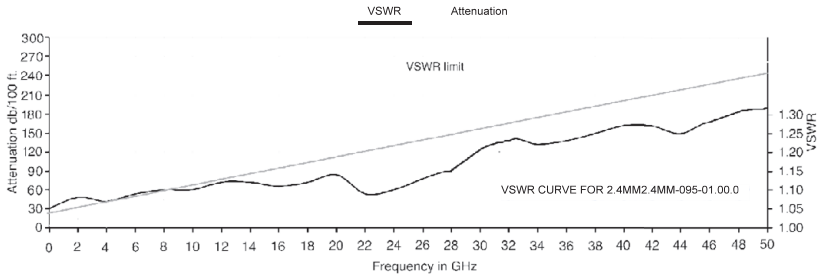
Operating Frequency DC-40.0 GHz



2.9MM MALE TO 2.9MM MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
2.9MM2.9MM-095-00.06.0	2.9MM PLUG to 2.9MM PLUG	0.6	\$88.00	\$87.00	\$86.00
2.9MM2.9MM-095-01.00.0		1.0	\$88.00	\$87.00	\$86.00
2.9MM2.9MM-095-01.06.0		1.5	\$90.50	\$89.50	\$88.50
2.9MM2.9MM-095-02.00.0		2.0	\$93.00	\$92.00	\$91.00
2.9MM2.9MM-095-02.06.0		2.5	\$95.50	\$94.50	\$93.50
2.9MM2.9MM-095-03.00.0		3.0	\$98.00	\$97.00	\$96.00
2.9MM2.9MM-095-04.00.0		4.0	\$105.00	\$104.00	\$103.00
2.9MM2.9MM-095-05.00.0		5.0	\$110.00	\$109.00	\$108.00
2.9MM2.9MM-095-06.00.0		6.0	\$115.00	\$114.00	\$113.00

Operating Frequency DC-50.0 GHz



2.4MM MALE TO 2.4MM MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-9	10-24	25-49
2.4MM2.4MM-095-00.06.0	2.4MM PLUG to 2.4MM PLUG	0.6	\$100.00	\$99.00	\$98.00
2.4MM2.4MM-095-01.00.0		1.0	\$100.00	\$99.00	\$98.00
2.4MM2.4MM-095-01.06.0		1.5	\$102.50	\$101.50	\$100.50
2.4MM2.4MM-095-02.00.0		2.0	\$105.00	\$104.00	\$103.00
2.4MM2.4MM-095-02.06.0		2.5	\$107.50	\$106.00	\$105.50
2.4MM2.4MM-095-03.00.0		3.0	\$110.00	\$109.00	\$108.00
2.4MM2.4MM-095-04.00.0		4.0	\$115.00	\$114.00	\$113.00
2.4MM2.4MM-095-05.00.0		5.0	\$120.00	\$119.00	\$118.00
2.4MM2.4MM-095-06.00.0		6.0	\$125.00	\$124.00	\$123.00

United Microwave Products Inc.

Direct Sales, Tech Support and Current Order Status

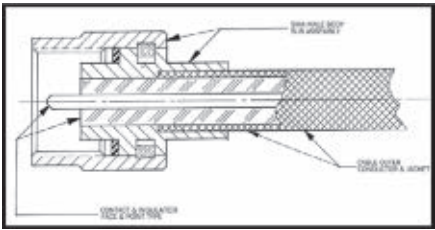
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MICROFORM 139

Operating Frequency DC-26.0 GHz

MICROFORM 139 is a hand formable replacement for .141 semi-rigid cable. Easily formed by hand, it's shape is retained with no spring back. Available as pre-made assemblies with SMA connectors. MICROFORM 139 cables are economical replacements for semi-rigid. **Contact Factory for Connectors and Electrical Performance not listed.**



ELECTRICAL PROPERTIES

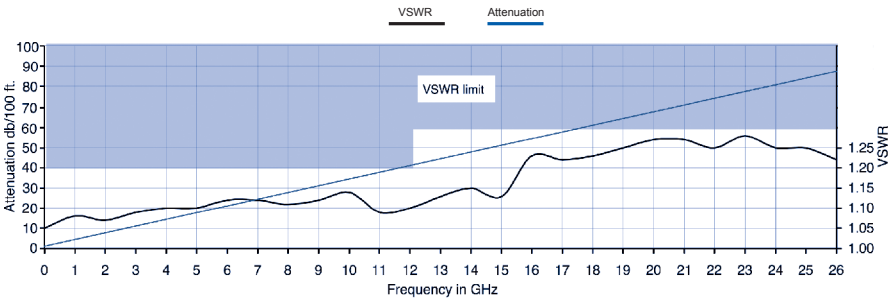
Impedance	50 ± 1 OHM
velocity of propagation	69.5%
Cut off Frequency	35.0 GHz
Max Operating Voltage	1900 Volts RMS
Nominal Capacitance	29.4 p/f
RF Shielding	Greater than 90db

MATERIALS

Inner Conductor	SIL. PLT. Cu Clad Steel.036 Dia.
Dielectric	PTFE .116 Dia.
Outer Conductor	Cu/Sn Composite Shield 100% Coverage .139 Dia. Nominal

MECHANICAL PROPERTIES

Bend Radius	Minimum 0.25 Inch
Weight	.3 oz/ft
Temp Range	-55°F/+400°F



SMA MALE TO SMA MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-24	24-49	50-99
AA-139-00.06.0	SMA PLUG to SMA PLUG	0.6	\$26.00	\$25.00	\$24.00
AA-139-01.00.0		1.0	\$26.00	\$25.00	\$24.00
AA-139-01.06.0		1.5	\$27.50	\$26.50	\$25.50
AA-139-02.00.0		2.0	\$29.00	\$28.00	\$27.00
AA-139-02.06.0		2.5	\$30.50	\$29.50	\$28.50
AA-139-03.00.0		3.0	\$32.00	\$31.00	\$30.00
AA-139-04.00.0		4.0	\$35.00	\$34.00	\$33.00
AA-139-05.00.0		5.0	\$38.00	\$37.00	\$36.00
AA-139-06.00.0		6.0	\$41.00	\$40.00	\$39.00

United Microwave Products Inc.

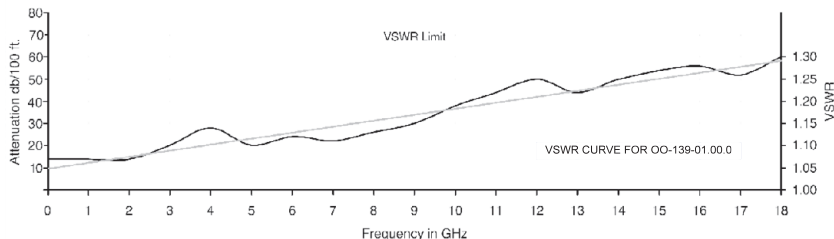
Direct Sales, Tech Support and Current Order Status

60 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 60

Prices listed effective as of 1 July 2008 and subject to change at any time.

MICROFORM 139

Operating Frequency DC-18.0 GHz



SMA MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
AO-139-00.06.0	SMA PLUG to TYPE "N" PLUG	0.5	\$49.00	\$48.00	\$44.00
AO-139-01.00.0		1.0	\$49.00	\$48.00	\$44.00
AO-139-01.06.0		1.5	\$50.50	\$49.50	\$45.50
AO-139-02.00.0		2.0	\$52.00	\$51.00	\$47.00
AO-139-02.06.0		2.5	\$53.50	\$52.50	\$48.50
AO-139-03.00.0		3.0	\$55.00	\$54.00	\$50.25
AO-139-04.00.0		4.0	\$58.00	\$57.00	\$53.75
AO-139-05.00.0		5.0	\$61.00	\$60.00	\$56.00
AO-139-06.00.0		6.0	\$64.00	\$63.00	\$59.00

SMA MALE TO TYPE N BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
AS-139-00.06.0	SMA PLUG to TYPE "N" BULKHEAD JACK	0.5	\$59.00	\$58.00	\$57.00
AS-139-01.00.0		1.0	\$59.00	\$58.00	\$57.00
AS-139-01.06.0		1.5	\$60.50	\$59.50	\$58.50
AS-139-02.00.0		2.0	\$62.00	\$61.00	\$60.00
AS-139-02.06.0		2.5	\$63.50	\$62.50	\$61.50
AS-139-03.00.0		3.0	\$65.00	\$64.00	\$63.00
AS-139-04.00.0		4.0	\$68.00	\$67.00	\$66.00
AS-139-05.00.0		5.0	\$71.00	\$70.00	\$69.00
AS-139-06.00.0		6.0	\$74.00	\$73.00	\$72.00

TYPE N MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
OO-139-00.06.0	TYPE "N" PLUG to TYPE "N" PLUG	0.5	\$46.00	\$45.00	\$47.00
OO-139-01.00.0		1.0	\$46.00	\$45.00	\$47.00
OO-139-01.06.0		1.5	\$47.50	\$46.50	\$48.50
OO-139-02.00.0		2.0	\$49.00	\$48.00	\$50.00
OO-139-02.06.0		2.5	\$50.50	\$49.50	\$51.50
OO-139-03.00.0		3.0	\$52.00	\$51.00	\$53.00
OO-139-04.00.0		4.0	\$55.75	\$54.75	\$56.00
OO-139-05.00.0		5.0	\$58.00	\$57.00	\$59.00
OO-139-06.00.0		6.0	\$61.00	\$60.00	\$62.00

SMA MALE TO SMA BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
AC-139-00.06.0	SMA PLUG to SMA BULKHEAD JACK	0.5	\$37.00	\$36.00	\$35.00
AC-139-01.00.0		1.0	\$37.00	\$36.00	\$35.00
AC-139-01.06.0		1.5	\$38.50	\$37.50	\$36.50
AC-139-02.00.0		2.0	\$40.00	\$39.00	\$38.50
AC-139-02.06.0		2.5	\$41.50	\$40.50	\$39.50
AC-139-03.00.0		3.0	\$43.00	\$42.00	\$41.00
AC-139-04.00.0		4.0	\$46.00	\$45.00	\$44.00
AC-139-05.00.0		5.0	\$49.00	\$48.00	\$47.00
AC-139-06.00.0		6.0	\$52.00	\$51.00	\$50.00

TYPE N MALE TO TYPE N BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
OS-139-00.06.0	TYPE "N" PLUG to TYPE "N" BULKHEAD JACK	0.5	\$66.75	\$65.75	\$64.75
OS-139-01.00.0		1.0	\$66.75	\$65.75	\$64.75
OS-139-01.06.0		1.5	\$67.50	\$66.50	\$65.50
OS-139-02.00.0		2.0	\$69.00	\$68.00	\$67.00
OS-139-02.06.0		2.5	\$70.50	\$69.50	\$68.50
OS-139-03.00.0		3.0	\$72.00	\$71.00	\$70.00
OS-139-04.00.0		4.0	\$75.80	\$74.80	\$72.80
OS-139-05.00.0		5.0	\$78.00	\$77.00	\$76.00
OS-139-06.00.0		6.0	\$81.00	\$80.00	\$79.00

MICROFORM 139

Operating Frequency DC-12.4 GHz

FURNISHED WITH CUBE TYPE RIGHT ANGLES

SMA MALE RIGHT ANGLE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH	1-24	25-49	50-99
BB-139-00.06.0	SMA PLUG RIGHT ANGLE to SMA PLUG RIGHT ANGLE	0.5 FL	\$46.00	\$45.00	\$44.00
BB-139-01.00.0		1.0 FL	\$46.00	\$45.00	\$44.00
BB-139-01.06.0		1.5 FL	\$47.50	\$46.50	\$45.50
BB-139-02.00.0		2.0 FL	\$49.00	\$48.00	\$47.00
BB-139-02.06.0		2.5 FL	\$50.50	\$49.50	\$48.50
BB-139-03.00.0		3.0 FL	\$52.00	\$51.00	\$50.00
BB-139-04.00.0		4.0 FL	\$55.00	\$54.00	\$53.00
BB-139-05.00.0		5.0 FL	\$58.00	\$57.00	\$56.00
BB-139-06.00.0		6.0 FL	\$61.00	\$60.00	\$59.00

SMA MALE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH	1-24	25-49	50-99
AB-139-00.06.0	SMA PLUG to SMA PLUG RIGHT ANGLE	0.5 FL	\$36.00	\$35.00	\$34.00
AB-139-01.00.0		1.0 FL	\$36.00	\$35.00	\$34.00
AB-139-01.06.0		1.5 FL	\$37.50	\$36.50	\$35.50
AB-139-02.00.0		2.0 FL	\$39.00	\$38.00	\$37.00
AB-139-02.06.0		2.5 FL	\$40.50	\$39.50	\$38.50
AB-139-03.00.0		3.0 FL	\$42.00	\$41.00	\$40.00
AB-139-04.00.0		4.0 FL	\$45.00	\$44.00	\$43.00
AB-139-05.00.0		5.0 FL	\$48.00	\$47.00	\$46.00
AB-139-06.00.0		6.0 FL	\$51.00	\$50.00	\$49.00

United Microwave Products Inc.

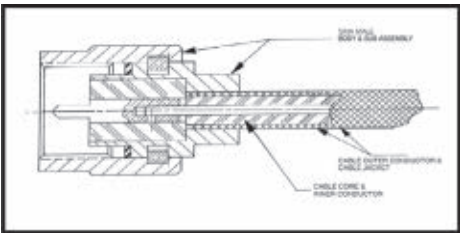
Direct Sales, Tech Support and Current Order Status

61 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 61

MICROFORM 088

Operating Frequency DC-26.0 GHz

MICROFORM 088 is a hand formable replacement for .085 semi-rigid cable. Easily formed by hand, it's shape is retained with no spring back. Available as pre-made assemblies with SMA connectors. MICROFORM 088 cables are economical replacements for semi-rigid. **Contact Factory for Connectors and Electrical Performance not listed.**



ELECTRICAL PROPERTIES

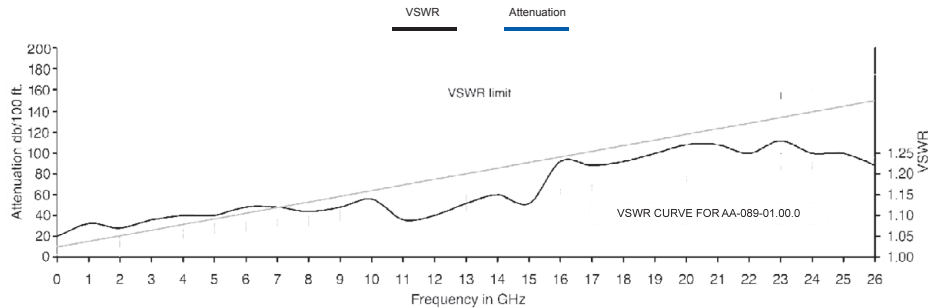
Impedance	50 ± 1 OHM
velocity of propagation	69.5%
Cut off Frequency	60.0 GHz
Max Operating Voltage	1200 Volts RMS
Nominal Capacitance	29.4 p/f
RF Shielding	Greater than 90db

MATERIALS

Inner Conductor	SIL PLT. Cu Clad Steel .020 Dia.
Dielectric	PTFE .066 Dia.
Outer Conductor	Cu/Sn Composite Shield 100% Coverage .088 Dia. Nominal

MECHANICAL PROPERTIES

Bend Radius	Minimum 0.5 Inch
Weight	.175 oz/ft
Temp Range	-55°F/+400°F



SMA MALE TO SMA MALE

PART NO.	CONNECTORS	LENGTH (Ft.)	1-24	24-49	50-99
AA-088-00.06.0	SMA PLUG to SMA PLUG	0.6	\$28.00	\$27.00	\$26.00
AA-088-01.00.0		1.0	\$28.00	\$27.00	\$26.00
AA-088-01.06.0		1.5	\$29.50	\$28.50	\$27.50
AA-088-02.00.0		2.0	\$31.00	\$30.00	\$29.00
AA-088-02.06.0		2.5	\$32.50	\$31.50	\$30.50
AA-088-03.00.0		3.0	\$34.00	\$33.00	\$32.00
AA-088-04.00.0		4.0	\$37.00	\$36.00	\$35.00
AA-088-05.00.0		5.0	\$40.00	\$39.00	\$38.00
AA-088-06.00.0		6.0	\$43.00	\$42.00	\$41.00

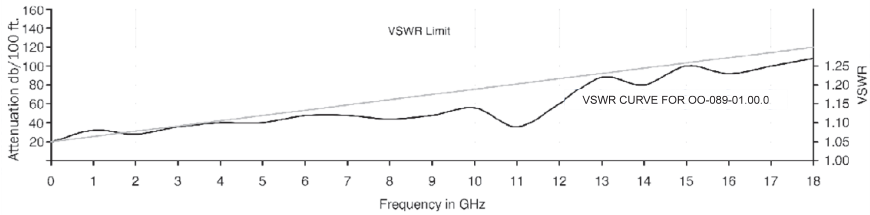
United Microwave Products Inc.

Direct Sales, Tech Support and Current Order Status

Prices listed effective as of 1 July 2008 and subject to change at any time.

MICROFORM 088

Operating Frequency DC-18.0 GHz



SMA MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
AO-088-00.06.0	SMA PLUG to TYPE "N" PLUG	0.5	\$51.00	\$50.00	\$46.00
AO-088-01.00.0		1.0	\$51.00	\$50.00	\$46.00
AO-088-01.06.0		1.5	\$52.50	\$51.50	\$47.50
AO-088-02.00.0		2.0	\$54.00	\$53.00	\$49.75
AO-088-02.06.0		2.5	\$55.50	\$54.50	\$50.00
AO-088-03.00.0		3.0	\$57.00	\$56.00	\$52.25
AO-088-04.00.0		4.0	\$60.00	\$59.00	\$55.75
AO-088-05.00.0		5.0	\$63.00	\$62.00	\$58.25
AO-088-06.00.0		6.0	\$66.00	\$65.00	\$61.00

SMA MALE TO TYPE N BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
AS-088-00.06.0	SMA PLUG to TYPE "N" BULKHEAD JACK	0.5	\$61.00	\$60.00	\$59.00
AS-088-01.00.0		1.0	\$61.00	\$60.00	\$59.00
AS-088-01.06.0		1.5	\$62.50	\$61.50	\$60.50
AS-088-02.00.0		2.0	\$64.00	\$63.00	\$62.00
AS-088-02.06.0		2.5	\$65.50	\$64.50	\$63.50
AS-088-03.00.0		3.0	\$67.00	\$66.00	\$65.00
AS-088-04.00.0		4.0	\$70.00	\$69.00	\$68.00
AS-088-05.00.0		5.0	\$73.50	\$72.50	\$71.50
AS-088-06.00.0		6.0	\$76.00	\$75.00	\$74.00

TYPE N MALE TO TYPE N MALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
OO-088-00.06.0	TYPE "N" PLUG to TYPE "N" PLUG	0.5	\$48.00	\$47.00	\$49.00
OO-088-01.00.0		1.0	\$48.00	\$47.00	\$49.00
OO-088-01.06.0		1.5	\$49.50	\$48.50	\$50.50
OO-088-02.00.0		2.0	\$51.00	\$50.00	\$52.00
OO-088-02.06.0		2.5	\$52.50	\$51.50	\$53.50
OO-088-03.00.0		3.0	\$54.00	\$53.00	\$55.00
OO-088-04.00.0		4.0	\$57.00	\$56.25	\$58.00
OO-088-05.00.0		5.0	\$60.00	\$59.00	\$61.00
OO-088-06.00.0		6.0	\$63.00	\$62.00	\$64.00

SMA MALE TO SMA BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
AC-088-00.06.0	SMA PLUG to SMA BULKHEAD JACK	0.5	\$39.00	\$38.00	\$37.00
AC-088-01.00.0		1.0	\$39.00	\$38.00	\$37.00
AC-088-01.06.0		1.5	\$40.50	\$39.50	\$40.00
AC-088-02.00.0		2.0	\$42.00	\$41.00	\$41.00
AC-088-02.06.0		2.5	\$43.50	\$42.50	\$41.50
AC-088-03.00.0		3.0	\$45.00	\$44.00	\$43.00
AC-088-04.00.0		4.0	\$48.00	\$47.00	\$46.00
AC-088-05.00.0		5.0	\$51.00	\$50.00	\$49.00
AC-088-06.00.0		6.0	\$54.00	\$53.00	\$52.00

TYPE N MALE TO TYPE N BULKHEAD FEMALE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
OS-088-00.06.0	TYPE "N" PLUG to TYPE "N" BULKHEAD JACK	0.5	\$68.75	\$67.75	\$66.75
OS-088-01.00.0		1.0	\$68.75	\$67.75	\$66.75
OS-088-01.06.0		1.5	\$69.50	\$68.50	\$67.50
OS-088-02.00.0		2.0	\$71.00	\$70.00	\$69.00
OS-088-02.06.0		2.5	\$72.50	\$71.50	\$70.50
OS-088-03.00.0		3.0	\$74.00	\$73.00	\$72.00
OS-088-04.00.0		4.0	\$77.00	\$76.00	\$75.00
OS-088-05.00.0		5.0	\$80.00	\$79.00	\$78.00
OS-088-06.00.0		6.0	\$83.00	\$82.00	\$81.00

MICROFORM 088

Operating Frequency DC-12.4 GHz

FURNISHED WITH CUBE TYPE RIGHT ANGLES

SMA MALE RIGHT ANGLE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
BB-088-00.06.0	SMA PLUG RIGHT ANGLE to SMA PLUG RIGHT ANGLE	0.5	\$48.00	\$47.00	\$46.00
BB-088-01.00.0		1.0	\$48.00	\$47.00	\$46.00
BB-088-01.06.0		1.5	\$49.50	\$48.50	\$47.50
BB-088-02.00.0		2.0	\$51.00	\$50.00	\$49.00
BB-088-02.06.0		2.5	\$52.50	\$51.50	\$50.50
BB-088-03.00.0		3.0	\$54.00	\$53.00	\$52.00
BB-088-04.00.0		4.0	\$57.00	\$56.00	\$55.00
BB-088-05.00.0		5.0	\$60.00	\$59.00	\$58.00
BB-088-06.00.0		6.0	\$63.00	\$62.00	\$61.00

SMA MALE TO SMA MALE RIGHT ANGLE

PART NO.	CONNECTORS	LENGTH (FL)	1-24	25-49	50-99
AB-088-00.06.0	SMA PLUG to SMA PLUG RIGHT ANGLE	0.5	\$38.00	\$37.00	\$36.00
AB-088-01.00.0		1.0	\$38.00	\$37.00	\$36.00
AB-088-01.06.0		1.5	\$39.50	\$38.50	\$37.50
AB-088-02.00.0		2.0	\$41.00	\$40.00	\$39.00
AB-088-02.06.0		2.5	\$42.50	\$41.50	\$40.50
AB-088-03.00.0		3.0	\$44.00	\$43.00	\$42.00
AB-088-04.00.0		4.0	\$46.00	\$45.00	\$44.00
AB-088-05.00.0		5.0	\$50.00	\$49.00	\$48.00
AB-088-06.00.0		6.0	\$53.00	\$52.00	\$51.00

United Microwave Products Inc.

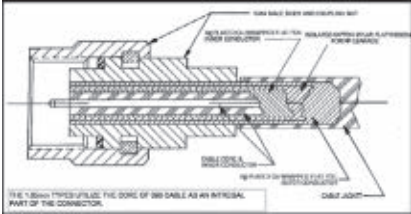
Direct Sales, Tech Support and Current Order Status

63 22129 S.Vermont Ave. Torrance CA. 90502 Phone (310) 320-1244 Fax (310) 320-9729 Email umpinc@pacbell.net 63

MICROFLEX 098

Operating Frequency DC-65.0 GHz

MICROFLEX 098 Flexible Cable Assemblies. These Cable Assemblies are available with 1.85mm "V"® Male Connectors with performance to 65 GHz ("V" is Registered Trademark of the ANRITSU Company) Contact **UNITED MICROWAVE PRODUCTS INC.** Phone(310)-320-1244 Fax (310)-320-9729 Web <http://www.unitedmicrowave.com> Email umpinc@pacbell.net for other types of Precision Cables



ELECTRICAL PROPERTIES

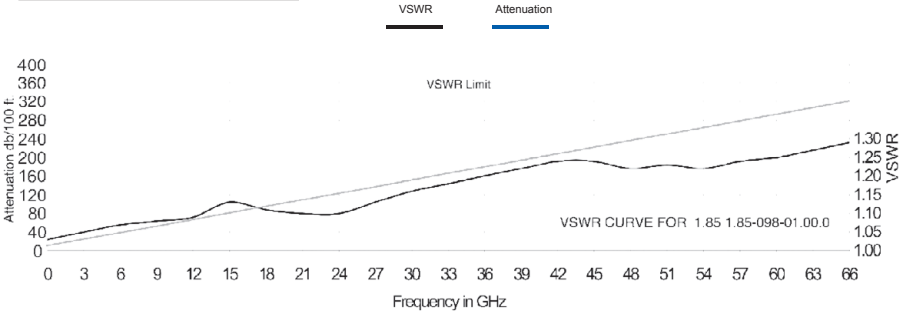
Impedance	50 ± 2 OHMs
Cut off Frequency	65.0 GHz
Nominal Capacitance	29.4 p/ft
Velocity of propagation	69.5%
Max Operating Voltage	1200 Volts RMS
RF Shielding	Greater than 90db

MATERIALS

Inner Conductor	SIL PLT Cu Clad Steel .0196 Dia.
Dielectric	Solid PTFE .062 Dia.
Outer Conductor	Dual SIL PLT Copper Ribbon Isolated By Mylar For RF Leakage .080 Dia.
Jacket	FEP Teflon .098 Dia.

MECHANICAL PROPERTIES

Bend Radius	Minimum 0.5 Inch
Temp Range	-55°F/+400°F
Weight	.175 oz/ft



1.85MM MALE TO 1.85MM MALE

PART NO.	CONNECTORS	LENGTH (FL)	1-9	10-24	25-49
1.85MM1.85MM-098-00.06.0	1.85mm M / 1.85mm M	0.6	\$112.00	\$111.00	\$110.00
1.85MM1.85MM-098-01.00.0	1.85mm M / 1.85mm M	1.0	\$112.00	\$111.00	\$110.00
1.85MM1.85MM-098-01.06.0	1.85mm M / 1.85mm M	1.5	\$114.50	\$113.50	\$112.50
1.85MM1.85MM-098-02.00.0	1.85mm M / 1.85mm M	2.0	\$117.00	\$116.00	\$113.00
1.85MM1.85MM-098-02.06.0	1.85mm M / 1.85mm M	2.5	\$119.50	\$118.50	\$117.50
1.85MM1.85MM-098-03.00.0	1.85mm M / 1.85mm M	3.0	\$122.00	\$121.00	\$120.00
1.85MM1.85MM-098-04.00.0	1.85mm M / 1.85mm M	4.0	\$127.00	\$126.00	\$125.00
1.85MM1.85MM-098-05.00.0	1.85mm M / 1.85mm M	5.0	\$132.00	\$131.00	\$130.00
1.85MM1.85MM-098-06.00.0	1.85mm M / 1.85mm M	6.0	\$137.00	\$136.00	\$135.00

United Microwave Products Inc.

Direct Sales, Tech Support and Current Order Status

COPY THIS FORM AND FAX, MAIL OR CONTACT FACTORY

EASY ORDER FORM

ORDER FORM MUST BE FILLED OUT COMPLETELY

DATE: _____ P.O. # _____

COMPANY: _____

STREET: _____

CITY: _____ STATE _____ ZIP _____

MINIMUM ORDER IS \$ 100.00 U.S.
ALL SALES ARE FINAL!
CONTACT FACTORY FOR DETAILS



()



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FOR RESALE, PLEASE ATTACH RESALE CERTIFICATE OR
ENTER YOUR RESELLER'S PERMIT NUMBER IN THE SPACE
BELOW AND SIGN THE ORDER

SELLER'S PERMIT # _____

CREDIT CARD ACCOUNT NUMBER

CARD SECURITY CODE (LAST 3 OR 4 DIGITS ON BACK OF CARD)

EXPIRATION DATE

CARDHOLDER'S NAME (PLEASE PRINT OR TYPE)

CARDHOLDER'S REGISTERED MAILING ADDRESS IF
DIFFERENT FROM ABOVE.

NAME _____

COMPANY _____

ADDRESS _____

CITY _____ STATE _____ ZIP _____

ITEM NO.	QUANTITY	UNITED MICROWAVE PRODUCTS INC. PART NO.	UNIT PRICE	EXTENDED PRICE
1				
2				
3				
4				
5				
6				
7				
8				
9				
10				

YOUR UPS
ACCOUNT NUMBER _____

FRIIGHT CHARGES WILL BE ADDED IF BLANK

() UPS GROUND

() UPS BLUE (2 day)

() UPS RED (overnight)

() UPS ORANGE (3 day)

SUB-TOTAL OF ORDER
MINIMUM ORDER IS \$100.00 U.S.

8.25% SALES TAX
CA RESIDENTS ONLY

SHIPPING CHARGES

TOTAL PRIOR TO SHIPPING
CHARGES BEING ADDED

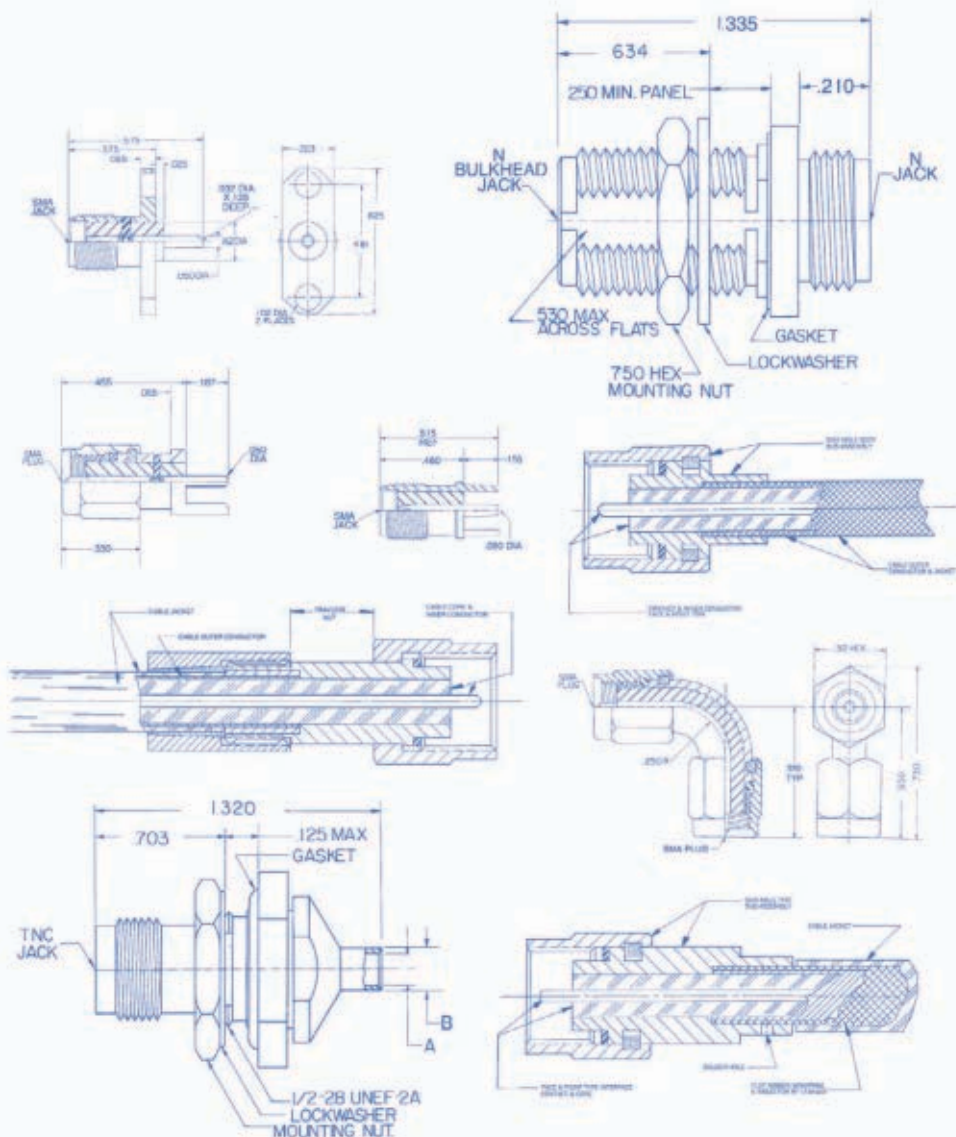
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